

# wireless world

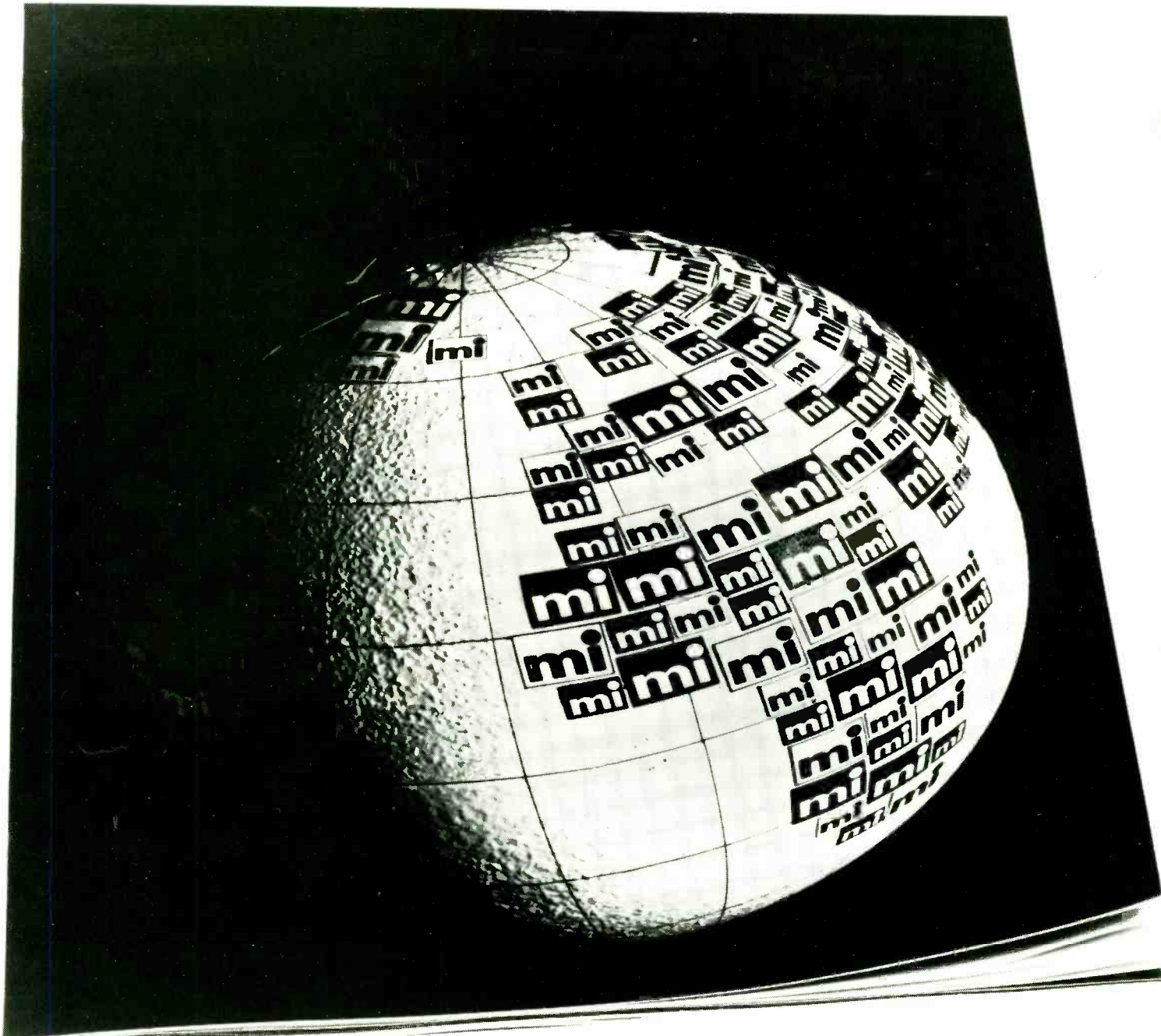
JULY 1975 30p

**Digital wristwatch**  
**Active notch filters**



Australia \$1.00  
Belgium Fr. 61.50  
Canada \$1.25  
Denmark Kr. 11.00  
Finland J. mk 5.00  
Germany DM. 4.00  
Greece Dr. 40.00  
Holland Dfl. 4.50  
Italy L.900  
Malaysia MS\$ 3.25  
New Zealand \$1.00  
Nigeria 25k  
Norway Kr. 10.00 incl. 10 pins  
Portugal Esc. 35.00  
South Africa 98 Cents  
Spain Ptas 80.00  
Sweden Kr. 6.00 incl. 10 pins  
Switzerland Fr. 5.80  
U.S.A. \$1.50





## Cover Story

Some Marconi Instruments are designed to be mobile. Others are not – but do a lot of travelling all the same. In fact, nearly three-quarters of **mi**'s total sales stem from export orders.

So there are plenty of people in Milwaukee or Mannheim or Melbourne or Montevideo who are just as discerning about Marconi Instruments as you are. And they're equally enthusiastic about **mi** service, too. We've service organisations in New Jersey, Munich, Paris and a whole lot of other

places to see to that.

There are **mi** distributors and representatives in more than 60 countries throughout the world and we have 14 associated companies in Africa, the Middle, Near and Far East, North and South America and Europe.

**mi**, then, doesn't only cover all the intricacies of planning and producing some of the world's finest electronic testing and measuring instruments . . . .

It covers the world, as well.

## **mi**: THE INTERNATIONALISTS

MARCONI INSTRUMENTS LIMITED

Longacres • St. Albans • Hertfordshire AL4 0JN • England • Telephone: St. Albans 59292 • Telex: 23350

A GEC-Marconi Electronics company.

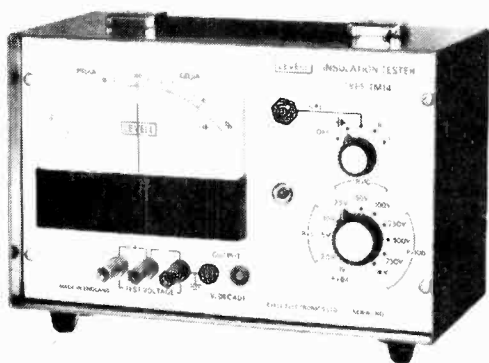
# LOW COST TESTERS



## LEVELL

### PORTABLE INSTRUMENTS

#### INSULATION TESTER



A logarithmic scale covering 6 decades is used to display either insulation resistance or leakage current at a fixed stabilised test voltage. The current available is limited to a maximum value of 3mA for safety and capacitors are automatically discharged when the instrument is switched off or to the CAL condition. The instrument operates from a 9V internal battery.

##### RESISTANCE RANGES

10M  $\Omega$  to 10T  $\Omega$  ( $10^{13}$   $\Omega$ ) at 250V, 500V, 750V and 1kV.

1M  $\Omega$  to 1T  $\Omega$  at 25V, 50V and 100V.

100k  $\Omega$  to 100G  $\Omega$  at 2.5V, 5V and 10V.

10k  $\Omega$  to 10G  $\Omega$  at 1V.

Accuracy  $\pm 15\%$  +800  $\Omega$  on 6 decade logarithmic scale.

Accuracy of test voltages  $\pm 3\%$   $\pm 50$ mV at scale centre.

Fall of test voltages  $< 2\%$  at 10 $\mu$ A and  $< 20\%$  at 100 $\mu$ A.

Short circuit current between 500 $\mu$ A and 3mA.

##### CURRENT RANGE

100pA to 100 $\mu$ A on 6 decade logarithmic scale.

Accuracy of current measurement  $\pm 15\%$  of indicated value.

Input voltage drop is approximately 20mV at 100pA, 200mV at 100nA and 400mV at 100 $\mu$ A.

Maximum safe continuous overload is 50mA.

##### MEASUREMENT TIME

$< 3$ s for resistance on all ranges relative to CAL position.

$< 10$ s for resistance of 10G  $\Omega$  across 1 $\mu$ F on 50V to 500V.

Discharge time to 1% is 0.1s per  $\mu$ F on CAL position.

##### RECORDER OUTPUT

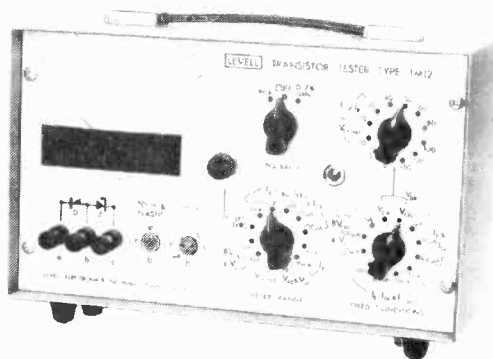
1V per decade  $\pm 2\%$  with zero output at scale centre.

Maximum output  $\pm 3$ V. Output resistance 1k  $\Omega$ .

type  
TM14

**£88**

#### TRANSISTOR TESTER



Tests bipolar transistors, diodes and zener diodes. Measures leakage down to 0.5 nA at 2V to 150V. Current gains are checked from 1 $\mu$ A to 100mA. Breakdown voltages up to 100V are measured at 10 $\mu$ A, 100 $\mu$ A and 1mA. Collector to emitter saturation voltage is measured at 1mA, 10mA, 30mA and 100mA for  $I_C/I_B$  ratios of 10, 20, 30. The instrument is powered by a 9V battery.

##### TRANSISTOR RANGES (PNP OR NPN)

$I_{CBO}$  &  $I_{EBO}$ : 10nA, 100nA, 1 $\mu$ A, 10 $\mu$ A and 100 $\mu$ A f.s.d. acc.  $\pm 2\%$  f.s.d.  $\pm 1\%$  at voltages of 2V, 5V, 10V, 20V, 30V, 40V, 50V, 60V, 80V, 100V, 120V, and 150V acc.  $\pm 3\%$   $\pm 100$ mV up to 10 $\mu$ A with fall at 100 $\mu$ A  $< 5\%$  +250mV.

$BV_{CBO}$ : 10V or 100V f.s.d. acc.  $\pm 2\%$  f.s.d.  $\pm 1\%$  at currents of 10 $\mu$ A, 100 $\mu$ A and 1mA  $\pm 20\%$ .

$I_B$ : 10nA, 100nA, 1 $\mu$ A ... 10mA f.s.d. acc.  $\pm 2\%$  f.s.d.  $\pm 1\%$  at fixed  $I_E$  of 1 $\mu$ A, 10 $\mu$ A, 100 $\mu$ A, 1mA, 10mA, 30mA, and 100mA acc.  $\pm 1\%$ .

$h_{FE}$ : 3 inverse scales of 2000 to 100, 400 to 30 and 100 to 10 convert  $I_B$  into  $h_{FE}$  readings.

$V_{BE}$ : 1V f.s.d. acc.  $\pm 20$ mV measured at conditions on  $h_{FE}$  test.

$V_{CE(sat)}$ : 1V f.s.d. acc.  $\pm 20$ mV at collector currents of 1mA, 10mA, 30mA and 100mA with  $I_C/I_B$  selected at 10, 20 or 30 acc.  $\pm 20\%$ .

##### DIODE & ZENER DIODE RANGES

$I_{DR}$ : As  $I_{EBO}$  transistor ranges.

$V_Z$ : Breakdown ranges as  $BV_{CBO}$  for transistors.

$V_{DF}$ : 1V f.s.d. acc.  $\pm 20$ mV at  $I_{DF}$  of 1 $\mu$ A, 10 $\mu$ A, 100 $\mu$ A, 1mA, 10mA, 30mA and 100mA.

type  
TM12

**£88**

### LEVELL ELECTRONICS LTD.

Moxon Street, High Barnet, Herts. EN5 5SD  
Tel: 01-449 5028/440 8686

Prices include batteries and U.K. delivery, V.A.T. extra. Optional extras are leather cases and mains power units. Send for data covering our range of portable instruments.

# SYSTEM 2000

# VORTEXION

A new range of sound equipment from **Vortexion, System 2000** has been designed by our engineers to combine the aesthetics of design in the domestic equipment field with the near flexibility of a modular system. Like all our equipment **Vortexion System 2000** is built to last.

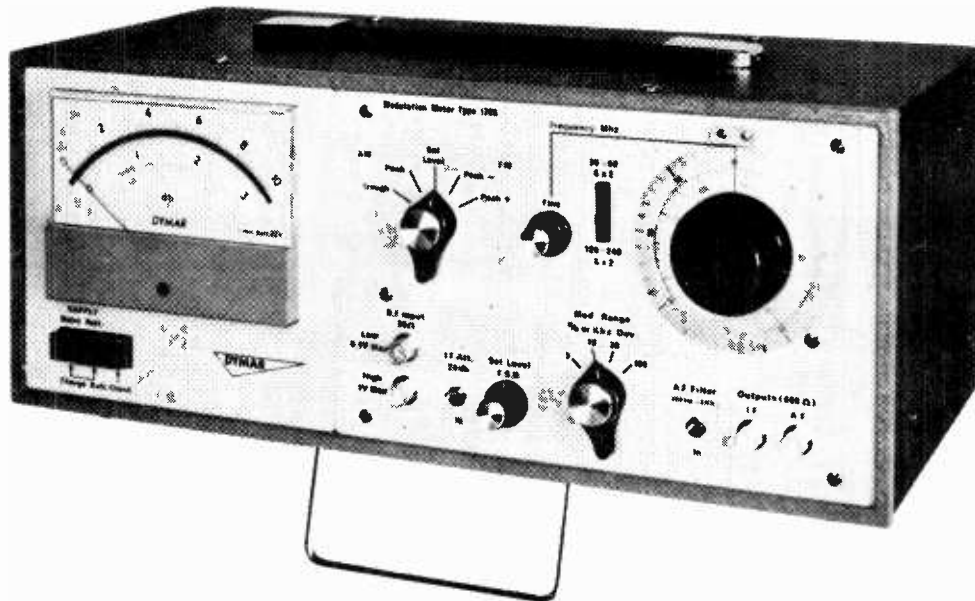
No matter what your sound problem, whether hotel or local pop group, ask our Design Consultants how it can be solved with **System 2000**.

**CSI VORTEXION** Vortexion Ltd., 257-263 The Broadway, Wimbledon, SW19 1SF  
Telephone: 01-542 2814 and 01-542 6242/3/4  
Telegrams: "Vortexion London SW19"

WW-064 FOR FURTHER DETAILS



# The Dymar 1785 portable AM-FM modulation meter.



## No need to ask who's in control. It's you!

The Dymar Type 1785 is quickly and easily tuneable anywhere across the entire VHF band and into UHF to encompass the mobile 470MHz band.

Designed to measure the depth of modulation or frequency deviation of today's demanding mobile and portable transmitters, the 1785 offers four ranges of both peak or trough percentage modulation (3% fsd to 100%) and both positive and negative deviation (3kHz to 100kHz).

The sensitivity over the entire frequency range is better than 2.5mV into 50 ohms (-40dbm),

which permits loose coupling to the transmitter under test. And internal noise is typically 44db below 3kHz.

Then, like most Dymar instruments, the 1785 is equally at home working from mains supply or in action in the field operating on its own rechargeable NiCd batteries.

With such value-for-money performance, you'll want to drive the 1785 to the limit – and that's why we emphasise that the 1785 is fully tuneable.

Want to know more? Use the Reader Reply Service or contact Dymar direct.

## **DYMAR**

**the name in radiotelephones**

*The Dymar range of instruments – designed for the mobile land, marine and air communications industry.*

DYMAR ELECTRONICS LIMITED,  
Colonial Way, Radlett Road, Watford,  
Herts. WD2 4LA, Telephone Watford 37321.  
Telex: 923035. Cables: Dymar Watford.

# Again and again and again

Given the time, the patience, and the money, one can connect\* fifty 303 amplifiers nose to tail so that the programme goes through one after the other gradually deteriorating along the way.

Deteriorating? The fact is, that apart from a very slight background hiss - akin to a good tape recording - the programme will sound exactly

the same at the end as when it started.

\*Of course one must fit an attenuator to reduce the signal back to its original level between each amplifier.

Send postcard for illustrated leaflet to Dept. WW  
Acoustical Manufacturing Co. Ltd.,  
Huntingdon PE18 7DB. Telephone (0480) 52561.

## QUAD

Products of The Acoustical Manufacturing Co. Ltd.

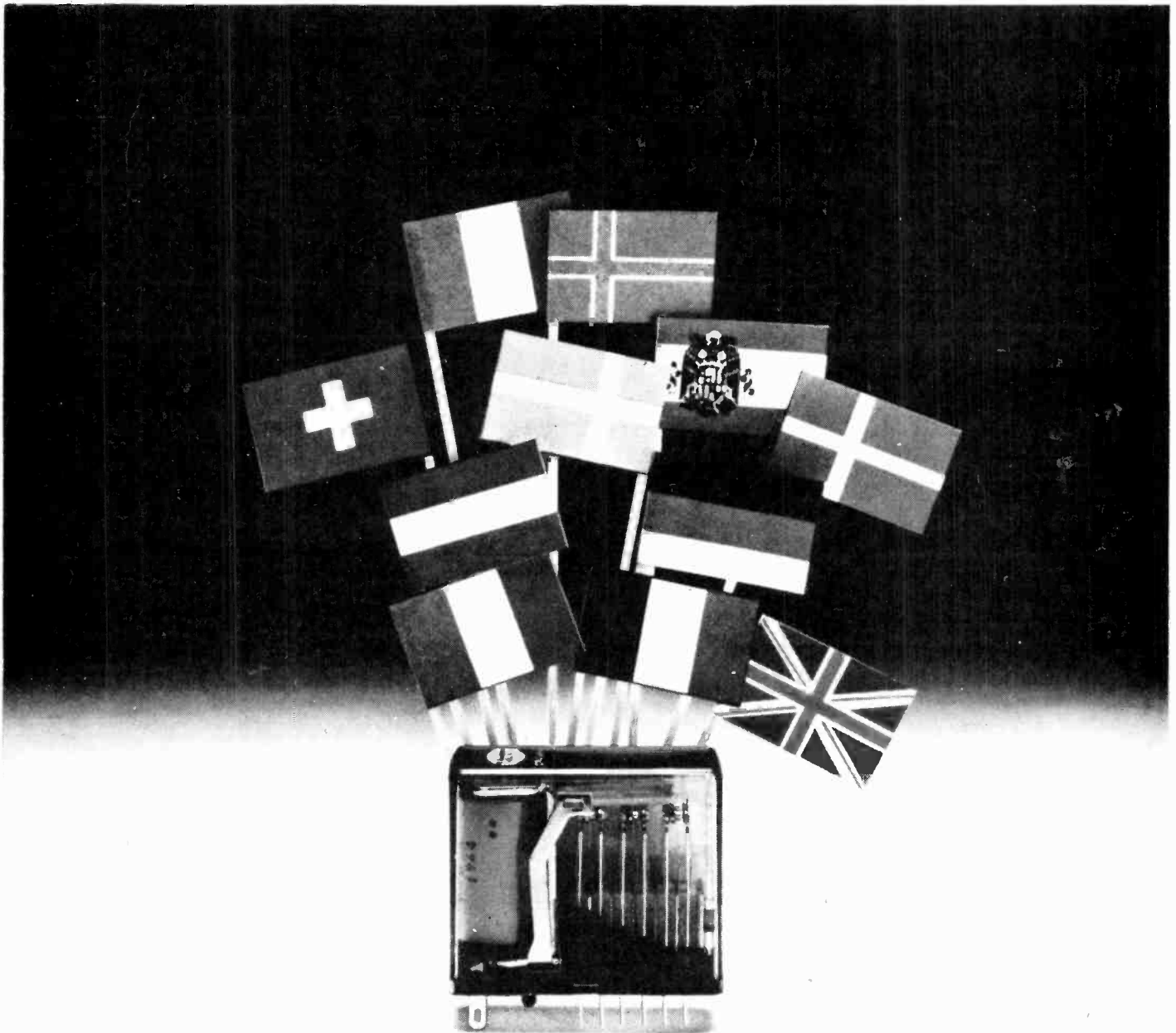
for the closest approach to the original sound

*QUAD is a Registered Trade Mark*



W/W-049 FOR FURTHER DETAILS





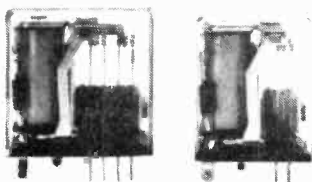
# Euro relay

**Varley is one of Europe's big names in miniature plug-in relays.**

The Miniaturised Bi-stable polarised relay type VPR and the P.O. approved relay type 23 are but two from a range used and approved throughout

the electronics world.

Each is built to uncompromising quality standards . . . with ultrasonic cleaning throughout coupled with exacting performance and timing checks.



**The same goes for our new AC range.**

These miniature plug-in relays have the same physical dimensions as the DC range. Shown: 2 and 4-contact versions. For all the help you need, contact Varley Technicians now - or send for the catalogue.

Oliver Pell Control Ltd.,  
Cambridge Row, Burrage Rd., Woolwich London SE18.  
Tel: 01-854 1422 Telex: 897071

Name \_\_\_\_\_

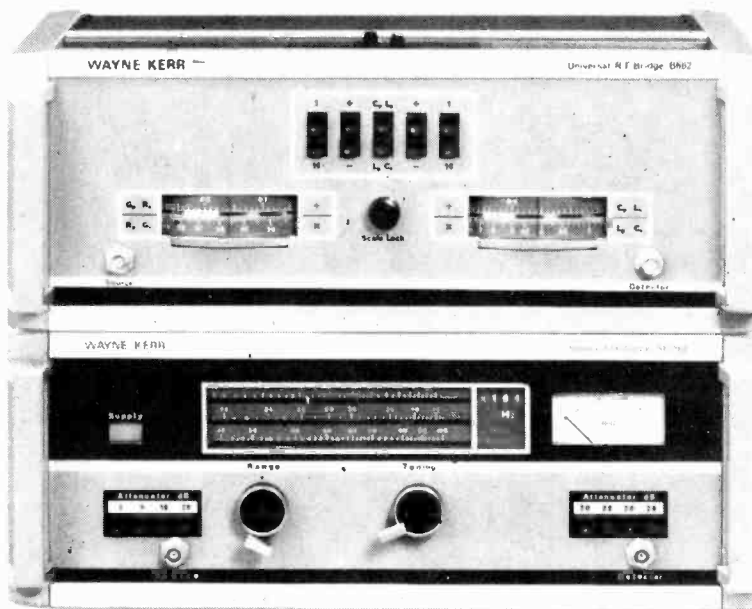
Company \_\_\_\_\_

Address \_\_\_\_\_

WW775

## Stable companions

# Wide-range universal bridge **B602** 0.1-100MHz source/detector **SR268** from Wayne Kerr



### SPECIFICATION

#### **B602**

Frequency range:	100kHz to 10MHz
Accuracy:	1% up to 3MHz, 1pF to 10nF 10Ω to 100kΩ 1μH to 10mH
Overall impedance range:	1fF to 1mF 100μΩ to 100MΩ (10nΩ to 10kΩ) 10pH to 10H

#### **SR268**

Frequency Range:	100kHz to 100MHz in 9 bands (SR268L 46.5kHz to 46.5MHz)
Frequency accuracy:	2-3% according to band used.
Short Term Frequency Stability:	0.01%
Output level:	0.5-2.0V according to band used.
Output attenuator:	3, 6, 10, 20 dB additive steps. 75Ω
Input sensitivity for 10% meter deflection:	1 to 30μV according to frequency setting
Input attenuator:	4 steps of 20 dB. 75Ω
Detector bandwidth:	2-3% according to band used

For more information, either phone Bognor Regis (02433) 25811 or write to the address below:

## **WAYNE KERR**

Durban Road, Bognor Regis, Sussex  
Telex: 86120. Cables: Waynkerr, Bognor

*A member of the Wilmot Breeden group*

The B602 transformer ratio arm bridge measures impedance in all four quadrants of the complex plane over the frequency range 100kHz to 10MHz. Because of novel features incorporated in the design, values from virtually a short circuit to an open circuit can be measured. This bridge has established a standard of performance and flexibility which is unobtainable from any other radio frequency bridge.

A standard inductor is included in the bridge network in addition to standards of capacitance and resistance enabling a periodic calibration of the scales which are correct at any frequency between 100kHz and 10MHz.

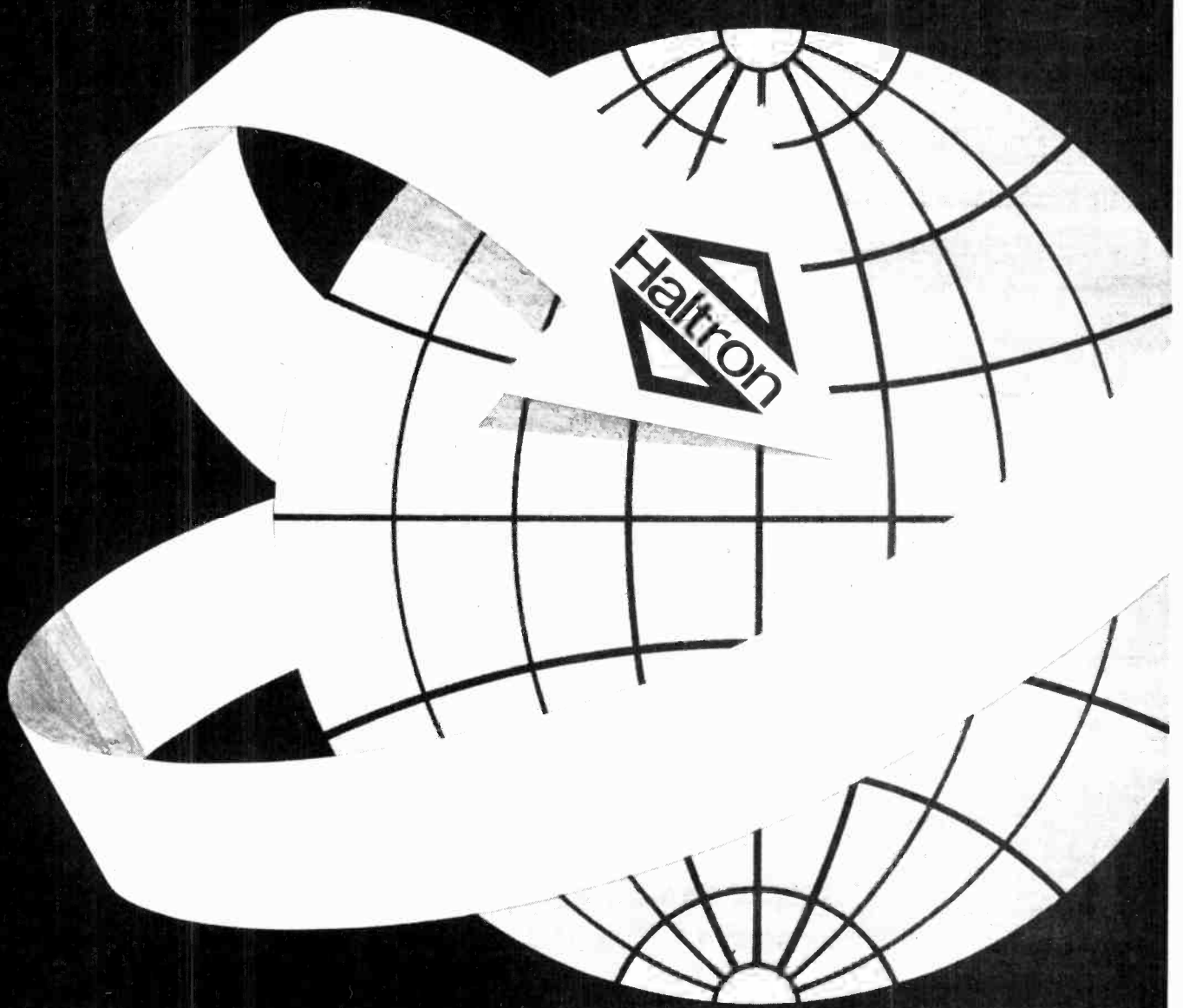
There are only two balance controls. One is direct reading in resistance and conductance, the other in capacitance and inductance and there is no interaction between them.

The stability realised allows a discrimination of 0.1% to be obtained for all types of measurement with a general accuracy of 1% over most of the impedance and frequency range.

The bridge is shown together with the SR268 Source and Detector which can also be used with other bridges in the Wayne Kerr range over the frequency band 100kHz to 100MHz. Nine frequency ranges are provided by this instrument and a single tuning control adjusts both source and detector to the exact frequency required.

Meticulous screening between the two sections provides freedom from bridge measurement errors due to leakage of the source signal into the detector. Common mode rejection transformers are incorporated in the input and output networks to reduce interference from unwanted signals, and push button attenuators are included to assist the logarithmic detector circuit to indicate approach of the bridge balance point.





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For high quality electronic valves, semiconductors and integrated circuits – and the speediest service – specify Haltron. It's the first choice of Governments and many other users throughout the world. Haltron product quality and reliability are clearly confirmed. The product range is very, very wide. And Haltron export expertise will surely meet your requirements. Wherever you are, get the best service. From Haltron.

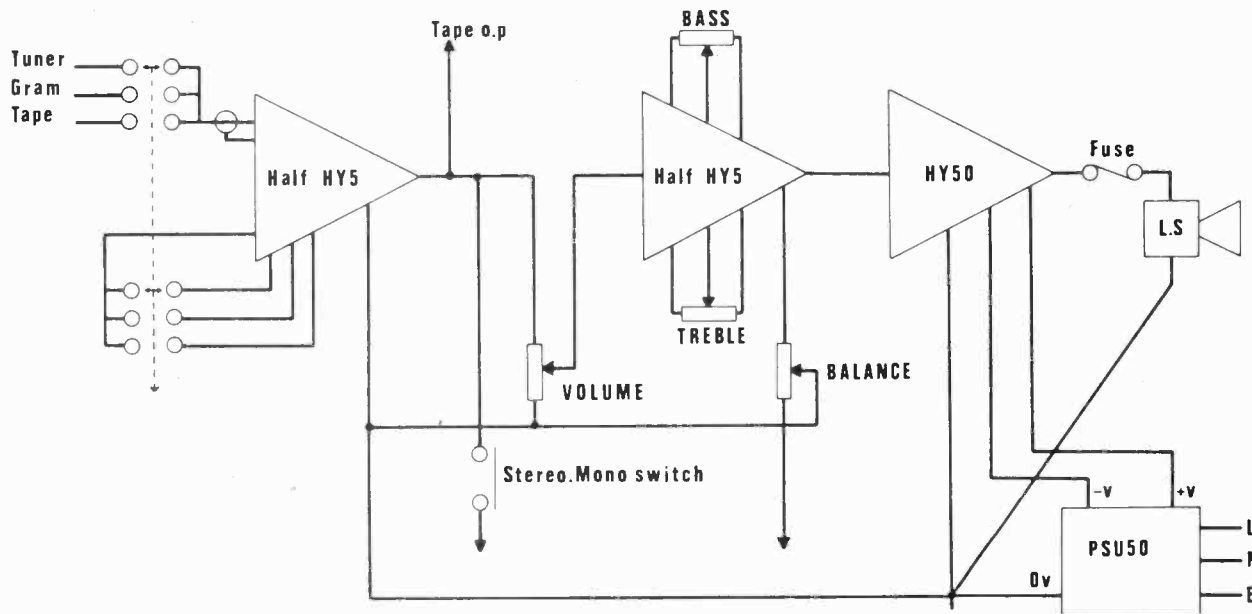


Hall Electric Limited,  
Electron House,  
Cray Avenue, St. Mary Cray,  
Orpington, Kent BR5 3QJ.  
Telephone : Orpington 27099  
Telex : 896141

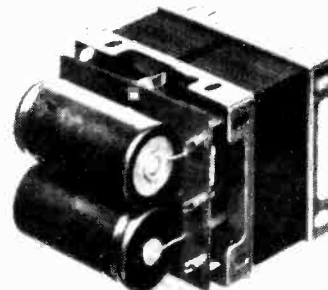
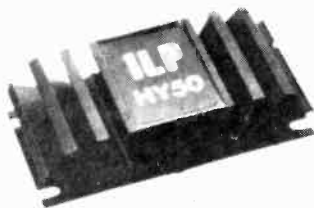
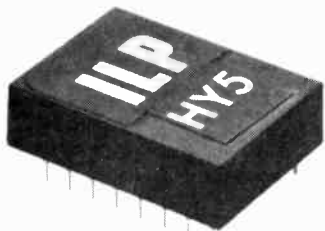
WW-005 FOR FURTHER DETAILS

# IP I.L.P. (Electronics) Ltd

## SHEER SIMPLICITY!



*Mono electrical circuit diagram with interconnections for stereo shown*



The HY5 is a complete mono hybrid preamplifier, ideally suited for both mono and stereo applications. Internally the device consists of two high quality amplifiers - the first contains frequency equalisation and gain correction, while the second caters for tone control and balance.

**TECHNICAL SPECIFICATION**

**Inputs**  
 Magnetic Pick-up 3mV, RIAA  
 Ceramic Pick-up 30mV  
 Microphone 10mV  
 Tuner 100mV  
 Auxiliary 3-100mV  
 Input impedance 47kΩ at 1kHz

**Outputs**  
 Tape 100mV  
 Main output 0db (0.775 volts RMS)

**Active Tone Control:**  
 Treble ±12db at 10kHz  
 Bass ±12db at 100Hz

**Distortion** 0.05% at 1kHz  
**Signal/Noise Ratio** 68db  
**Overload Capability** 40 db on most sensitive input

**Supply Voltage** 16-25 volts.  
 PRICE £4.75 + £1.19 V.A.T. P & P free.

The HY50 is a complete solid state hybrid Hi-Fi amplifier incorporating its own high conductivity heatsink hermetically sealed in black epoxy resin. Only five connections are provided: Input, output, power lines and earth.

**TECHNICAL SPECIFICATION**

**Output Power** 25 watts RMS into 8Ω  
**Load Impedance** 4-16Ω  
**Input Sensitivity** 0db (0.775 volts RMS)  
**Input Impedance** 47kΩ  
**Distortion** Less than 0.1% at 25 watts typically 0.05%  
**Signal/Noise Ratio** Better than 75db  
**Frequency Response** 10Hz - 50kHz ± 3db  
**Supply Voltage** 25 volts  
**Size** 105 x 50 x 25 mm.  
 PRICE £6.20 + £1.55 V.A.T. P & P free

The PSU50 incorporated a specially designed transformer and can be used for either mono or stereo systems.

**TECHNICAL SPECIFICATIONS**

**Output voltage** 50 volts (25-0-25)  
**Input voltage** 210-240 volts  
**Size** L.70. D.90. H.60 mm.  
 PRICE £6.25 + £1.56 V.A.T. P & P free

**TWO YEARS GUARANTEE ON ALL OUR PRODUCTS**

**I.L.P. Electronics Ltd,**  
**Crossland House,**  
**Nackington, Canterbury,**  
**Kent CT4 7AD**  
**Tel (0227) 63218**

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 Please debit my Access account  Barclay card account   
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 Name & Address \_\_\_\_\_  
 Signature \_\_\_\_\_



# r.f. test equipment

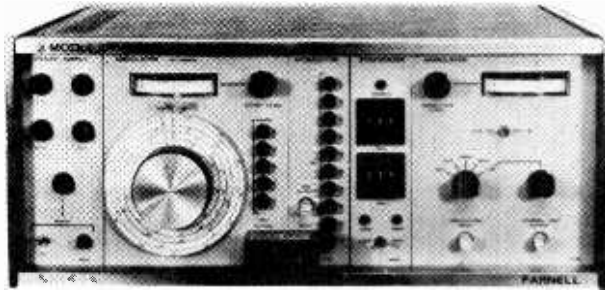
**TM6 R.F. MILLIVOLTMETER**  
1mV to 300V f.s.d.  
50kHz to 1.5GHz  
Useful to 3GHz  
Near true r.m.s. readings on low ranges



**WW—039 FOR FURTHER DETAILS**

A range of general purpose r.f. signal generators, synthesizers and sweepers is offered covering 100kHz to 512MHz. Specialist instruments include a Marine Test Set covering 0.1 to 12MHz for use with receivers with narrow i.f. filters for S.S.B. reception and u.h.f./v.h.f. Test Sets suitable for work on alerters, pocket pagers and two-way personal radios. All the equipment is programmable and may therefore be used in A.T.E. systems or operated manually.

Complementary r.f. test equipment includes an r.f. millivoltmeter, a programmable attenuator and an x-y recorder.



### MODULAR SIGNAL GENERATORS

100kHz to 12MHz M1A/ABM AM,FM Signal Generator	10MHz to 100MHz M2/ACM AM,FM Signal Generator
M1A/ADM Synthesised AM/FM Signal Generator	M2/ADM Synthesizer AM/FM Signal Generator
M1A/ACS Sweep Generator	M2/ACS Sweep Generator

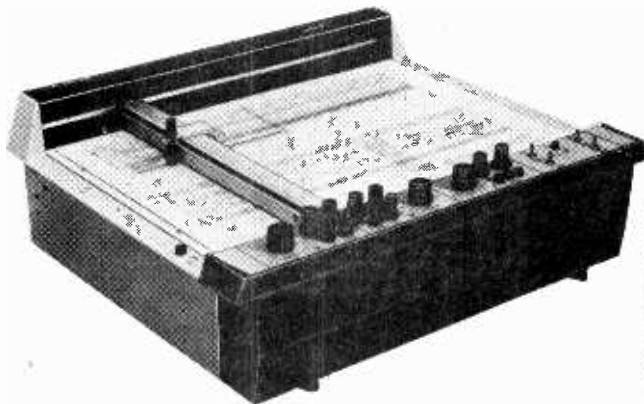
10MHz to 512MHz M3A/ABM AM FM Signal Generator
M3A/ACM Synthesized Signal Generator
M3A/ACS Sweep Generator

**WW—040 FOR FURTHER DETAILS**



**T6003 TEST SET**  
Synthesized signal generator 0.1 to 12MHz  
Accuracy 5PPM. Resolution 100Hz  
3 to 50Hz narrowband sweep Five settable markers  
A.M./F.M. capability Built-in detector

**WW—041 FOR FURTHER DETAILS**



**X-Y RECORDER**  
A3 Size flatbed Ideal for use with sweepers  
Also available with timebase for general use  
Electrostatic paper hold Disposable pens

**WW—042 FOR FURTHER DETAILS**



**PA112 ATTENUATOR**  
Manual or programmable operation  
0-122dB in 1dB steps  
Uses thick film technology and reed relay switching  
Small size  
Built-in power supply

**WW—043 FOR FURTHER DETAILS**

... from  Farnell

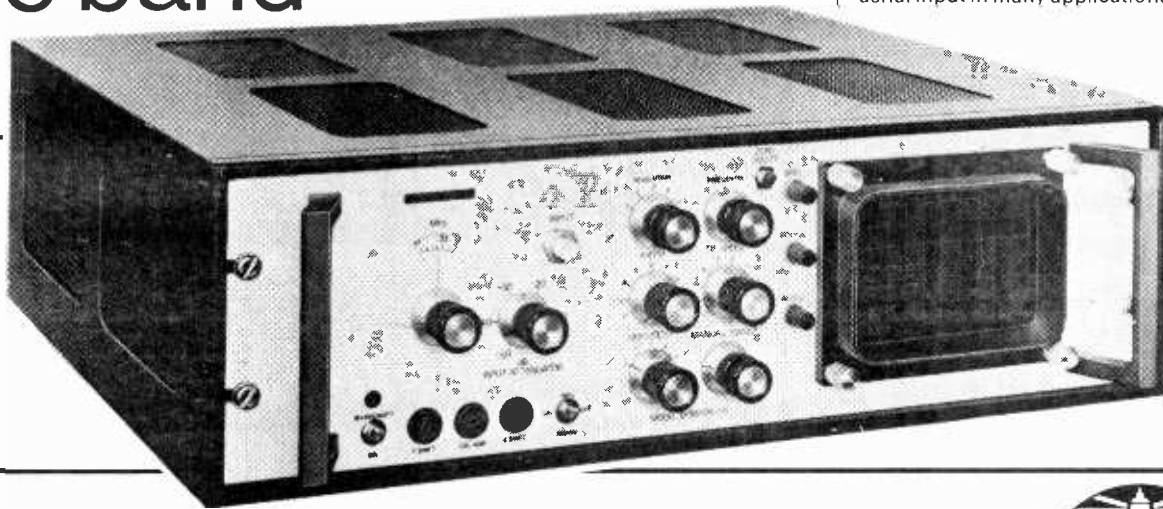
# A clear view of the band

Eddystone EP961 MkII Panoramic Display Units provide visual monitoring of all signals in a selected band.

MkII-A is tunable from 50kHz to 800kHz, matching the IFs used in MF and HF communication receivers.

MkII-B covers 500kHz to 36.5MHz. It is ideal for use with VHF and UHF receivers for monitoring FM broadcasts and communication transmissions, and its usefulness extends into the laboratory field.

Both versions can be used with direct aerial input in many applications.



## Eddystone Radio Limited

Member of Marconi Communication Systems Limited

Alvechurch Road, Birmingham B31 3PP, England  
Telephone: 021-475 2231 Telex: 337081

A GEC-Marconi Electronics Company

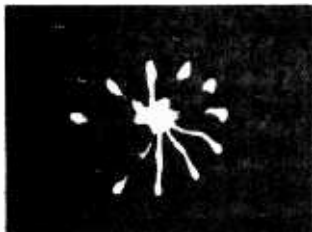


WW-024 FOR FURTHER DETAILS

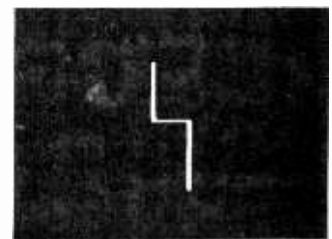
# RCA's new 3-inch scope... an entire servicing system



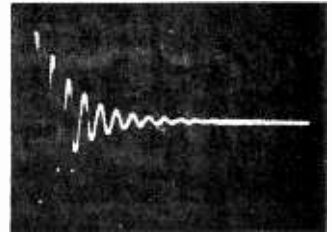
1. It's an 8MHz general purpose scope. Typical composite TV video signal.



3. It's a Vectorscope for colour TV AFP C alignment. Colour bar generator used for test signal.



2. It's a "Quicktracer" Transistor/Diode and Component Tester. Typical junction wave form.



4. It's a "ringing" tester for coils, yokes, transformers. Typical ringing test pattern.

5. It includes the WG-400A Direct Low-Capacitance Switch Probe and Cable with BNC type connector, and a special "Quicktracer" probe.

For full information on the new WO-33B, contact **RCA Electronic Components** Sunbury-on-Thames, Middlesex Tel: Sunbury 85511 or an appointed RCA (EC) Distributor:

**ELECTRONIC COMPONENT SUPPLIES (WINDSOR) Ltd**  
Thames Avenue, Windsor, Berkshire Tel: Windsor 68101

**EDMUNSON ELECTRONIC COMPONENTS Ltd** 30-50 Ossory Road, London SE1 5AN Tel: 01-237 0404

**BLACK ARROW ELECTRONICS Ltd** Millbrook Road, Yate, Bristol BS17 5NX. Tel: Chipping Sodbury 315824

WW-033 FOR FURTHER DETAILS

**RCA** Electronic Components





# Now suitable for U.K., European and American voltages...

Minimod, the versatile British range of encapsulated power supplies first introduced in 1973, has now been extended to cover European and North American mains voltages (and is interchangeable with most American types). Normally available ex-stock, all units are fully stabilised with fold back current limiting – the 5V models have over voltage crowbar too!

### STANDARD MODELS

Type Number	Output Voltage	Output Current Amps	Short Circuit Current mA (Typical)	% Regulation Line and Load (Typical)
PU01	5 ± 0.1	0.5	370	0.3
PU02	5 ± 0.1	1.0	770	0.5
PU03	15 - 0 - 15 ± 0.2	0.10	37	0.1
PU04	15 - 0 - 15 ± 0.2	0.20	84	0.1
PU05	12 - 0 - 12 ± 0.2	0.12	45	0.1
PU06	12 - 0 - 12 ± 0.2	0.24	120	0.2
PU11	18 - 0 - 18 ± 0.2	.15	50	0.1
PU10	15 ± 0.2	.10	37	0.1
PU12	12 ± 0.2	.10	45	0.1
PU13	18 ± 0.2	.065	23	0.1

Input voltage ranges 103 - 126V, 200 - 240V, 210 - 250V. Frequency 50 - 400 Hz all types.

Comprehensive specification given in brochure GT 29b which is available on request.

### ★ SPECIAL DESIGN SERVICE

Custom built units for applications requiring different specifications are produced as part of our standard service. Try us first.



Specialists in Electronic Transformers & Power Supplies.

# GARDNERS

TRANSFORMERS LIMITED

Gardners Transformers Limited, Christchurch, Dorset, BH23 3PN.  
Tel. Christchurch 2284 (STD 0201 5 2284) Telex. 41276 GARDNERS XCH  
WW—038 FOR FURTHER DETAILS

# NEW!...the decon-dalo 33 PC Quick -Dri etch -resist marker



A unique drafting aid for the electronics engineer enabling him to prepare in minutes a perfect PCB.

A fine-tipped marking pen charged with free-flowing etch-resist ink – new formulation QUICK-DRI ink is ready for etching in just two minutes!

Simply draw the desired circuit onto copper laminated board – etch – clean.

The circuit is ready to use

## NO MESS – NO MASKING A perfect circuit every time!

Still only £1.00 for one-off, £4.00 for six, £8.00 for twelve VAT and post extra. Available now in every country in Europe.

Decon Laboratories Ltd., Ellen Street, Portslade, Brighton BN4 1EQ Phone: 0273 414371

Please send me further details on the 33 PC Quick-Dri

Name .....

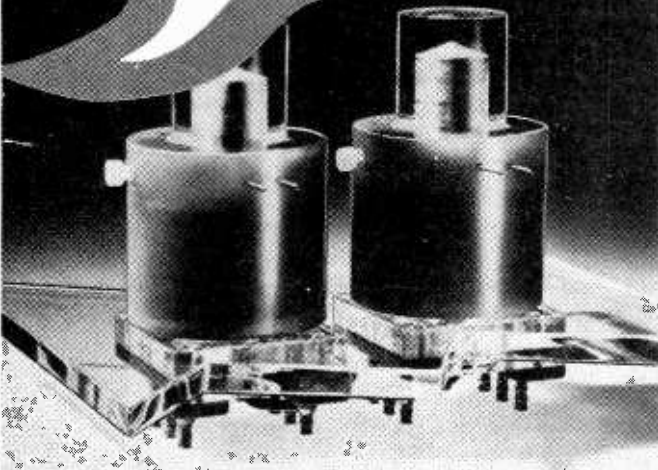
Address .....

Post to: DECON LABORATORIES LTD.  
FREEPOST

PORTSLADE, BRIGHTON, ENGLAND  
(No Stamp Needed) Phone 0273 414371

WW—052 FOR FURTHER DETAILS

*"He's asking  
for a  
reed relay  
assembly  
with a 30kV  
isolated coil"*



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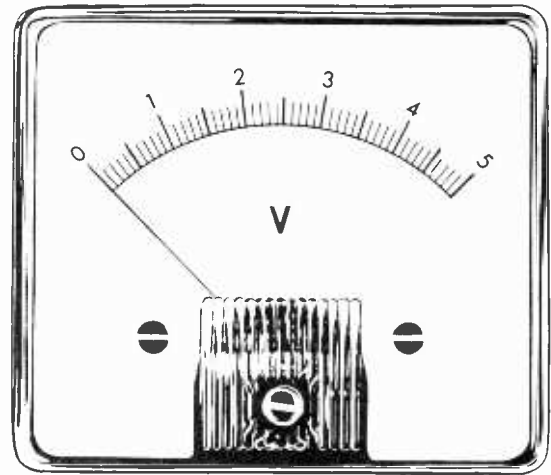
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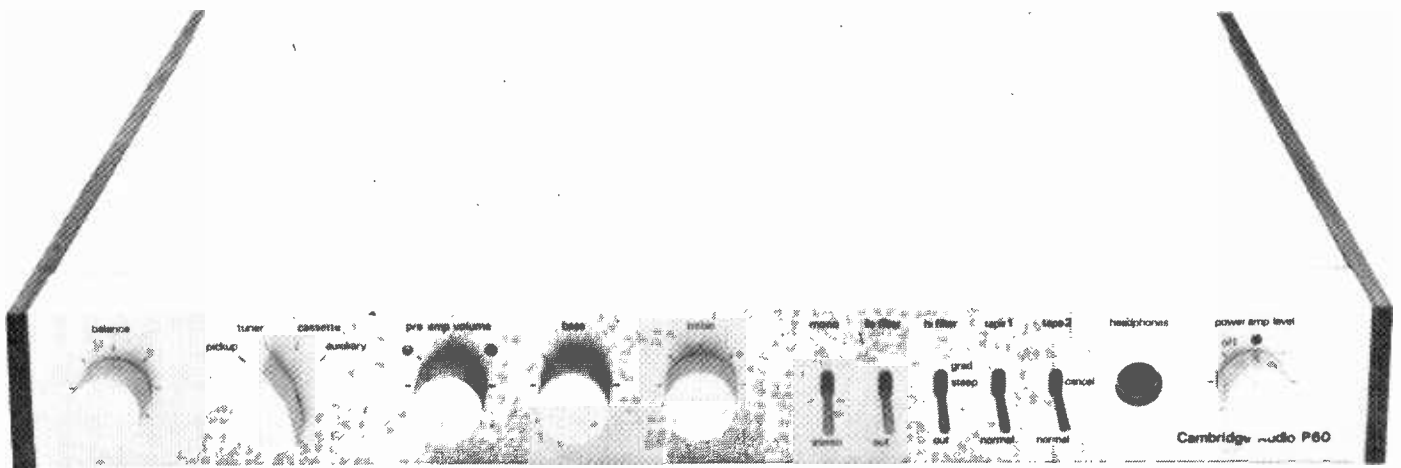
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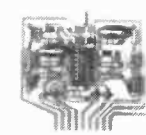
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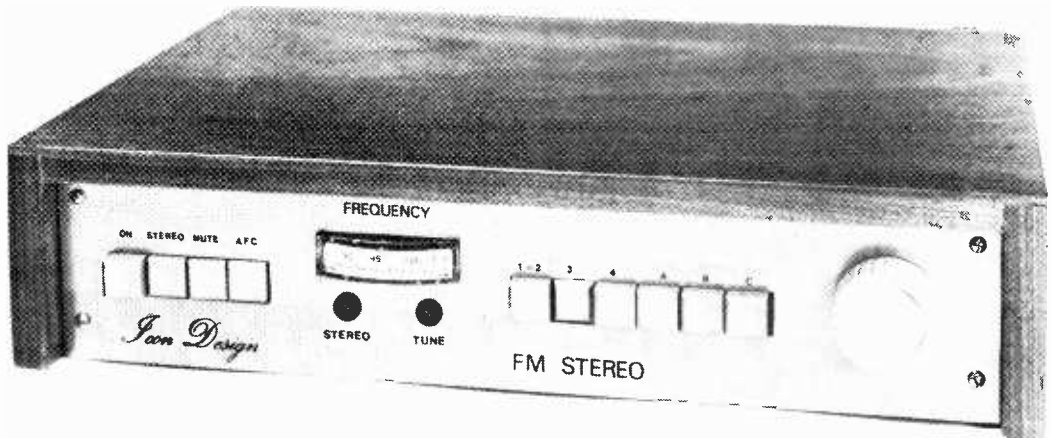


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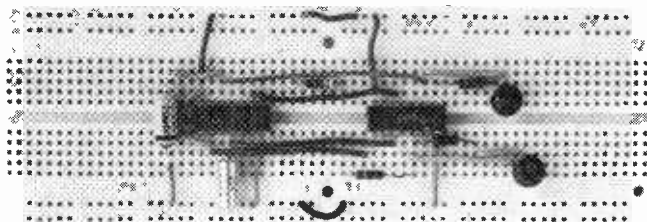
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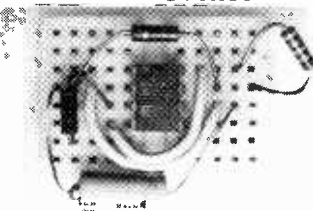
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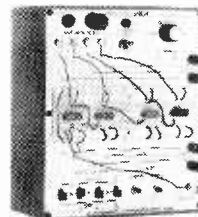
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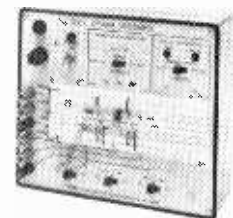
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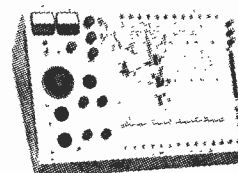


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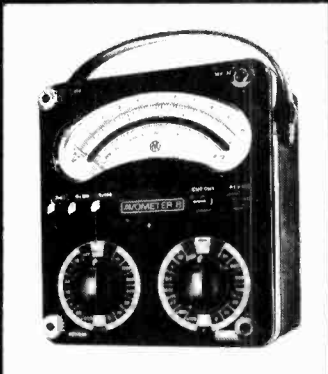
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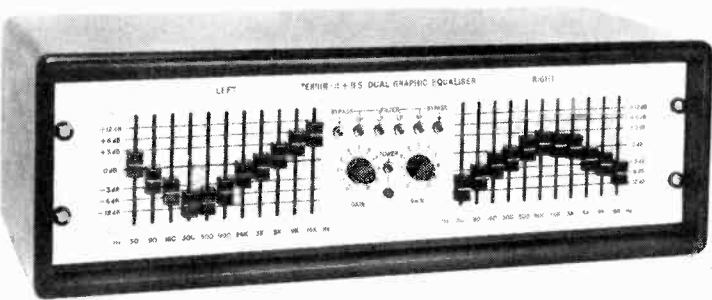
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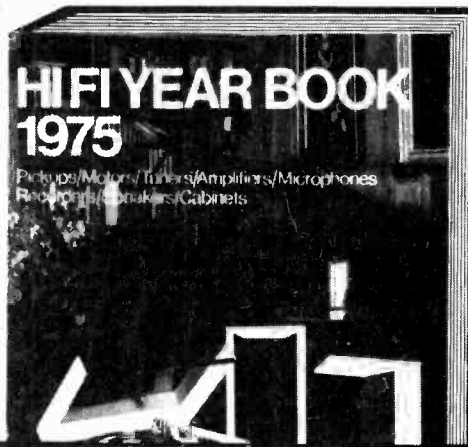
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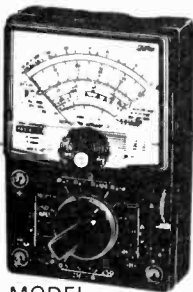
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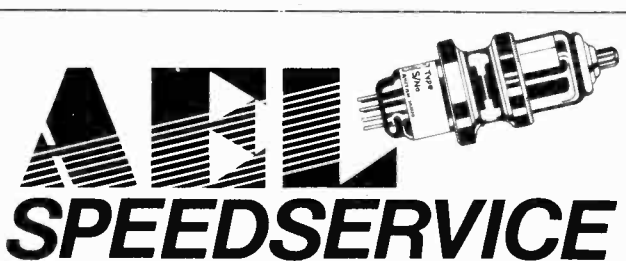
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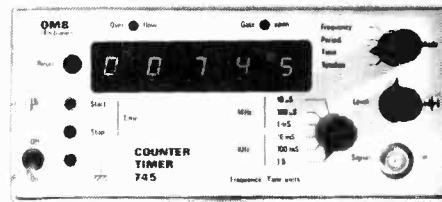
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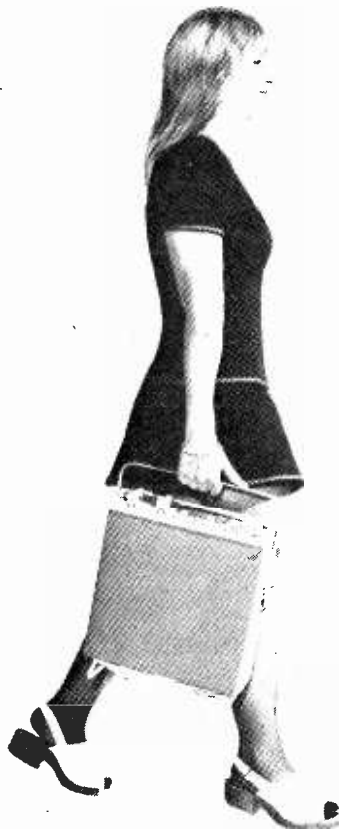


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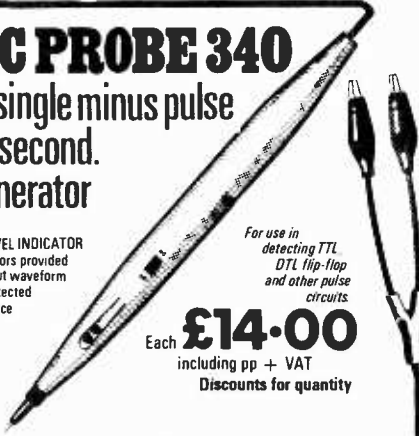
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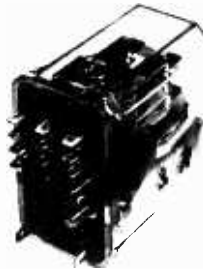
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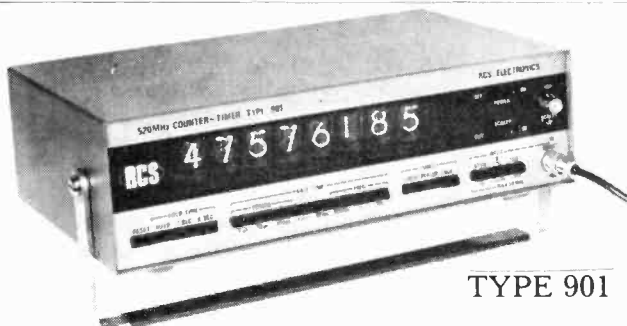
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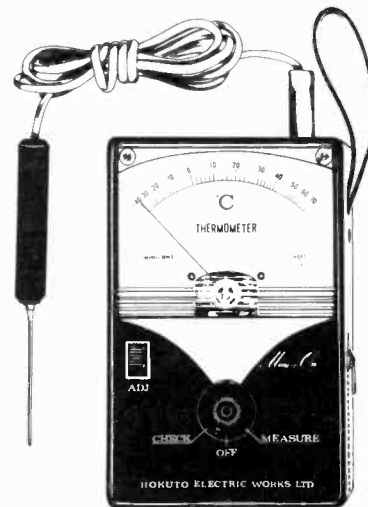
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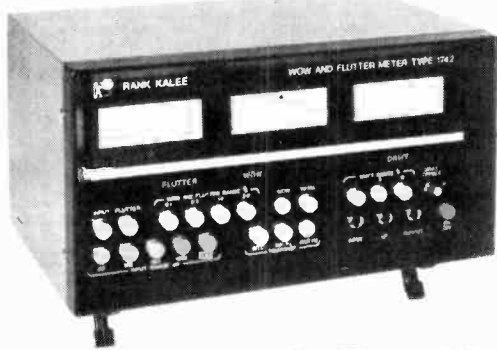
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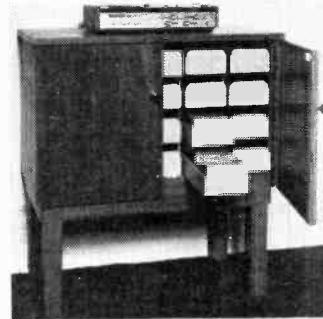
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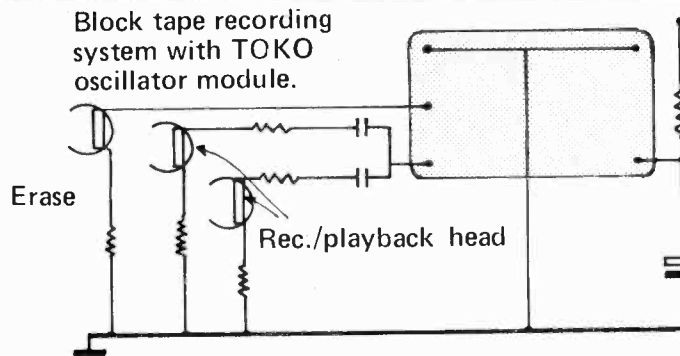
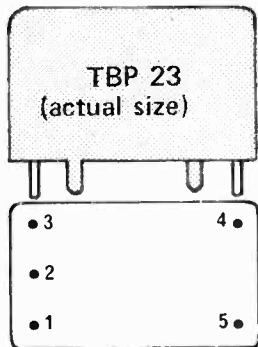


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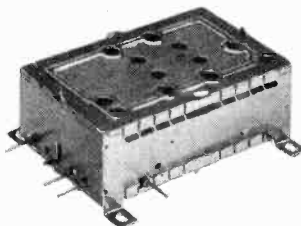
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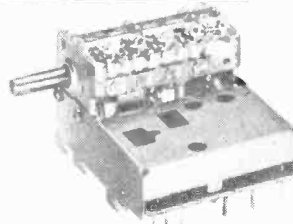
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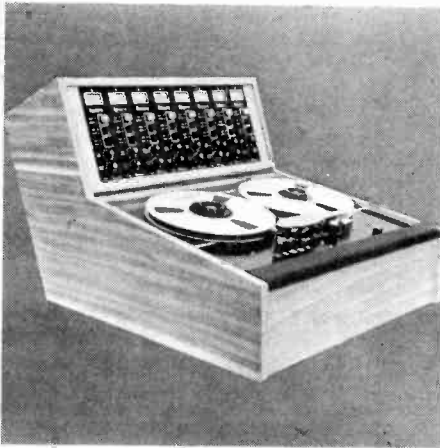


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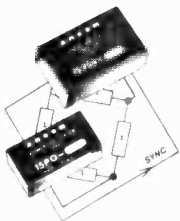
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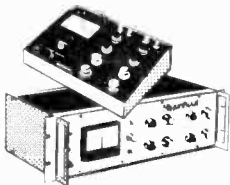
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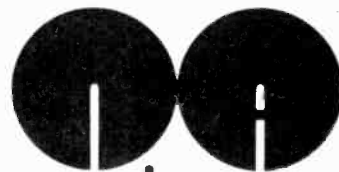
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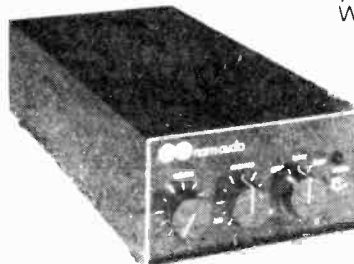


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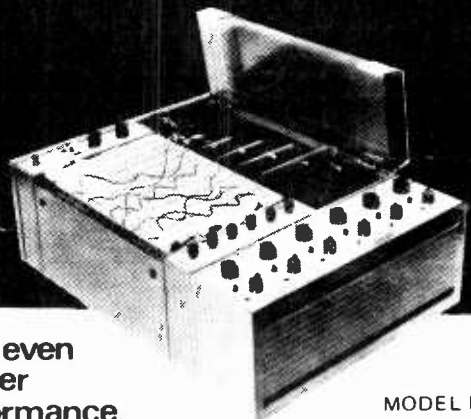
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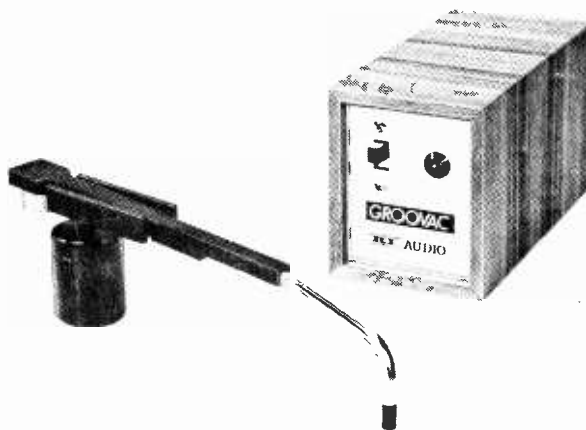
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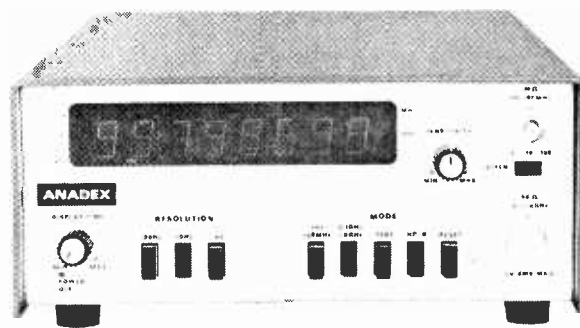
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## NEW PRODUCT

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**Brief Spec.** Amplifier: Low field Toroidal transformer, Mag. input, Tape In/Out facility (for noise reduction unit, etc), THD less than 0.1% at 20W into 8 ohms. All sockets, fuses, etc, are PC mounted for ease of assembly. Tuner section: uses Mullard LP1186 module requiring no RF alignment, ceramic IF, INTERSTATION MUTE, and phase-locked IC stereo decoder. LED tuning and stereo indicators. Tuning range 88–104MHz. 30dB mono S/N @ 1.8µV. THD typ. 0.4%.

**PRICE: £47.95 + 99p p&p + VAT.**



## NELSON-JONES STEREO FM TUNER

*A very high performance tuner with dual gate MOSFET RF and Mixer front end, triple gang varicap tuning, and dual ceramic filter/dual IC IF amp.*

**Brief Spec.** Tuning range 88–104MHz. 20dB mono quieting @ 0.75µV. Image rejection—70dB. IF rejection—85dB. THD typically 0.4%.

IC stabilized PSU and LED tuning indicators. Push-button tuning and AFC unit. Choice of either mono or stereo with a choice of stereo decoders.

**PRICE: Mono £25.46 + 85p p&p + VAT;**

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**With ICPL Decoder £29.73 + 85p p&p + VAT.**

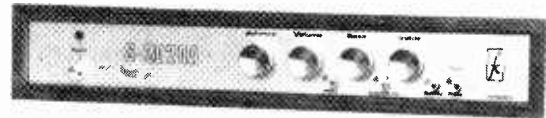
## NEW PRODUCT

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**Typ. Spec.** Sens. 30dB S/N mono @ 1.8µV. Tuning range 88–104MHz. LED sig. strength indicator. LED Stereo indicator. THD typically 0.4%.

**PRICE: Stereo £26.32 + 85p p&p + VAT. Mono £22.40 + 85p p&p + VAT.**

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### BASIC MODULE TUNER

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**PRICE: Mono £11.11 + 25p p&p + VAT; Stereo £13.89 + 25p p&p + VAT.**



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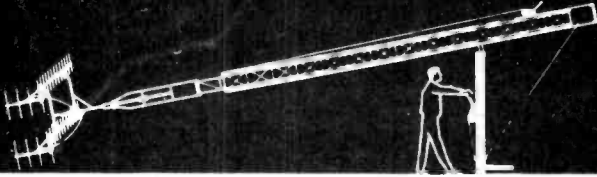
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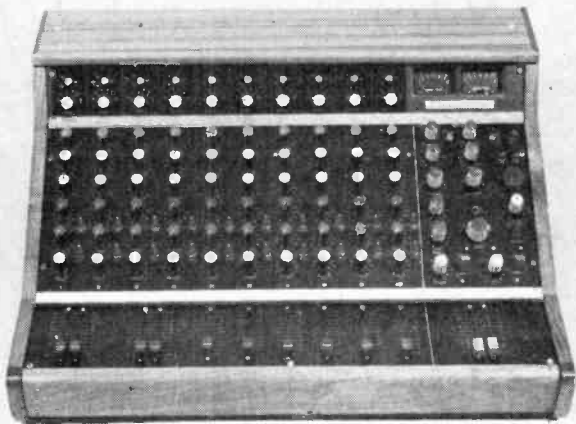
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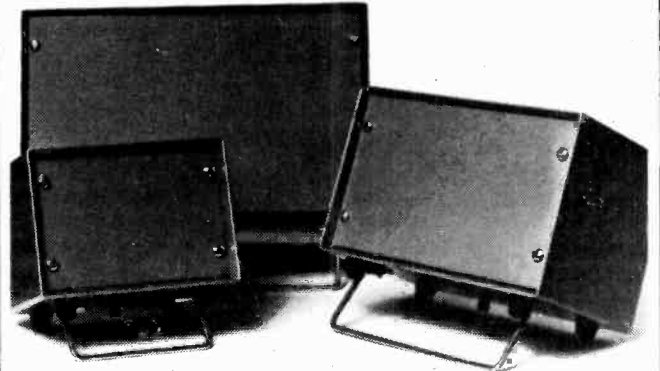
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22	8 1/2"	5 1/2"	5 1/2"	—	<b>4.01</b>	<b>0.82</b>
23	10 1/2"	6 1/2"	6 1/2"	—	<b>4.78</b>	<b>0.88</b>
24	12 1/2"	7 1/2"	7 1/2"	—	<b>5.22</b>	<b>0.88</b>
25A	6 1/2"	4 1/2"	4 1/2"	<b>3.46</b>	<b>3.90</b>	<b>0.82</b>
25B	6 1/2"	4 1/2"	6 1/4"	<b>3.63</b>	<b>4.07</b>	<b>0.82</b>
26A	8 3/4"	5 3/4"	6 1/4"	<b>4.89</b>	<b>5.33</b>	<b>0.88</b>
26B	8 3/4"	5 3/4"	8 1/4"	<b>5.11</b>	<b>5.55</b>	<b>0.88</b>
27A	12 1/4"	7 1/2"	5 1/2"	<b>5.33</b>	<b>5.88</b>	<b>0.88</b>
27B	12 1/4"	7 1/2"	8"	<b>5.77</b>	<b>6.32</b>	<b>0.88</b>
28A	14"	10 1/2"	6 1/2"	<b>6.32</b>	<b>6.87</b>	—
28B	14"	10 1/2"	8 1/2"	<b>6.87</b>	<b>7.42</b>	—
29A	10"	4"	6"	<b>4.40</b>	<b>4.84</b>	<b>0.88</b>
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62	17 1/2"	8 1/2"	9 1/2"	—	<b>9.24</b>	—
63	16 1/2"	9 1/2"	9 1/2"	—	<b>9.24</b>	—
64	15 1/2"	7 1/2"	12 1/2"	—	<b>9.24</b>	—
65	17 1/2"	8 1/2"	12 1/2"	—	<b>10.56</b>	—
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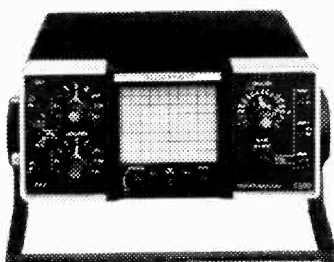
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of VAT

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# wireless world

**Electronics, Television, Radio, Audio**

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This month's front cover is a composite view of David Clegg's digital watch, a full description of which starts this month.

## IN OUR NEXT ISSUE

**Electronics and the railways**, a survey of past, present and future developments in communications from signalling to fail-safe systems in high-speed travel.

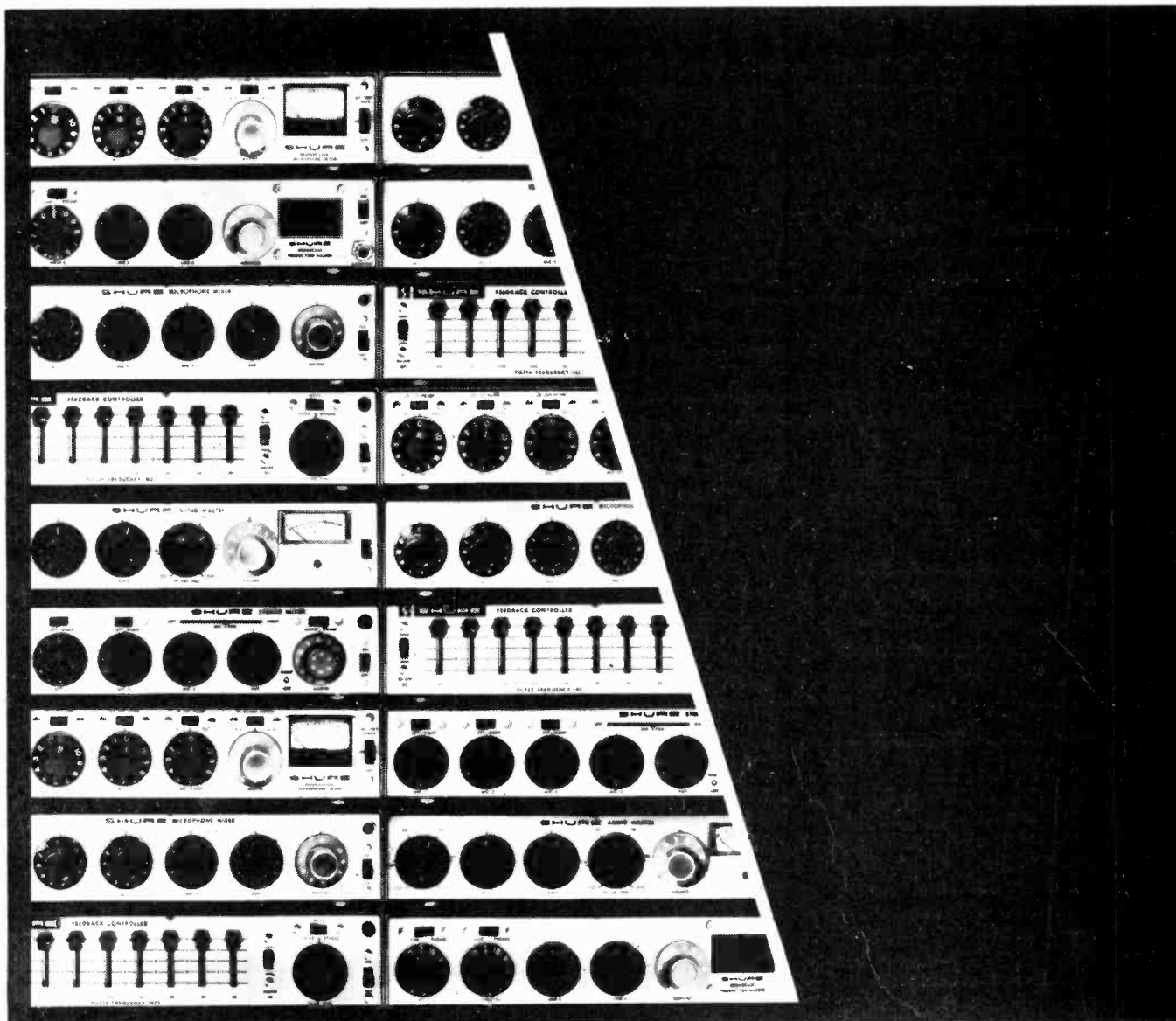
**Audio level meter.** Constructional design, using columns of l.e.d.s for logarithmic display, has characteristics similar to BBC peak programme meter.

**Solid-state wristwatch.** The second part of this unusual project gives the printed circuit board design and other constructional details.

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# wireless world

## The analogue to digital conversion

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Until about twenty years ago, the majority of measuring instruments displayed their results in an analogue manner, usually by means of a pointer meter. The accuracy of measuring electronics was such that the precision of this kind of indication was adequate. At this point, frequency measurement using flip-flops and logical gates came into large-scale use, and a numerical indication was the obvious way to display the reading. The numbers did not imply a spurious, mythical accuracy of measurement, because these instruments were capable of a high degree of accuracy.

Since then, measurement capabilities in many fields have improved and digital indication has been adopted to take advantage of this improvement. We have now reached the stage where an instrument is sometimes regarded as not quite "with it" unless a row of numbers appears on the front panel. Digital readout appears, in a sense, to have become a fashion and is sometimes used when the simpler pointer indication may have advantages. It ought to be remembered that the presentation of a measurement in numerical form does not mean that it is necessarily a more accurate measurement. It may give a more precise reading, but that is not to be confused with precision of measurement.

In some instances, a digital display can be a liability. Any slowly-varying quantity or a parameter which is only required to be known roughly is not a suitable case for the digital treatment. In the first instance the display may be a jumble of changing figures and in the second the display must be *read* rather than recognized. Clock faces, for instance, are very rarely read and are sometimes made without numerals: the position of the hands is taken in at a glance. Or again, a speedometer is usually an analogue indicator and one feels that any time spent reading numbers on a car dashboard would be better employed in looking where one is going, particularly while accelerating or decelerating, when the numerals on a digital indicator can be incomprehensible.

This is not, of course, a tirade against the superb digital instruments designed for precision voltage or frequency measurement — there is often no other way to present such readings. But a feeling persists that the humble moving-coil meter on the end of amplifying or impedance-changing electronics (or even displaying the results of measurements made by digital means, such as frequency) can still give a good account of itself.

Doubtless, many engineers who would consider themselves improperly dressed without an array of digital instruments in their equipment will disagree, pointing out that not only have we published a design for a digital speedo, but are now in the digital watch and clock business. We welcome their comments and, if they are sufficiently numerous and interesting to other readers, will publish a selection of them in a future issue.



# Solid-state digital wristwatch

C.m.o.s. circuitry and liquid-crystal display give long battery life 1 — Design

by D. D. Clegg

This article describes the design and construction of a wristwatch having a liquid crystal digital display and a quartz crystal time reference. The author was originally tempted to consider the design of a watch with a conventional display, i.e., one with hands driven by a sub-miniature stepping motor. This was later ruled out, however, because it involved a lot of conventional watchmaking expertise quite beyond the limited resources of the author.

## Design considerations

As a starting point, the following requirements were set down in order of importance:

- (1) The watch should be accurate; at least as accurate as a more conventional watch of equivalent price. The timing reference must, therefore, be a quartz crystal which will result in a stability of better than 1 second per day.
- (2) The finished watch should be a reasonably presentable piece of jewellery, i.e. it must not only look good, but also be a sensible size. The author had no intention of wearing a three-inch die-cast box on his wrist!
- (3) The display must be easy to read under all reasonable conditions of use.
- (4) The batteries must be easily obtainable and must last a sensible length of time. The absolute minimum acceptable battery life would be three months or, preferably, longer.

While compiling this list, the author was tempted to add a fifth requirement — that the watch should be easy to assemble — but later realised that this and requirement (2) are incompatible. It will become obvious during the course of this article that this design is very much a compromise because, in early 1974, there were very few suitable components available: all the major ones being imported from either the USA or Europe. For this reason the watch is quite difficult to construct and is, unfortunately, not suitable for economic manufacture in quantity. The watch described here can be built for around £50.

**Logic type.** Considerations of size and power consumption ruled out the use of

## SPECIFICATION

**Time reference:** 32.768kHz quartz crystal.

**Display:** field-effect liquid crystal.

**Power supply:** three RM312H mercury cells or WH1 watch cells. Typical life 1 year. (Minimum 9 months.)

**Stability:** better than 1s per day. typically 3 seconds per week.

**Size:** module diameter 31mm.

Depth of main part of module 7.3mm.

Depth of front part of module 1.75mm.

s.s.i. or m.s.i. bipolar logic for the watch: the only alternative was l.s.i./c.m.o.s. and at that time only one manufacturer's product was available in this country. This was the two-chip system designed for wristwatches with digital displays by Solid State Scientific Inc. One of the chips is a silicon gate c.m.o.s. oscillator and divider packaged in a ten-lead flat-pack — the SCL-5425-AF — and the other is an aluminium-gate watch circuit with outputs suitable for driving liquid-crystal displays, packaged in a 30-lead flat-pack — the SCL5424-F.

**Display.** After deciding on a digital display, the author's first intention had been to use an l.e.d. display and to provide a "Display" button to reduce power requirements, so that the display would draw power from the battery only when required. The SCL-5424-F watch chip will not drive an l.e.d. display directly and so it was decided to interface it with CD-4009 c.m.o.s. inverters. At that time, however, c.m.o.s. was in short supply, and c.m.o.s. in flat-packs (necessary because of the size) was almost completely unobtainable; delivery times in excess of six months being quoted in some cases.

The alternative was to use a liquid-crystal display which would require no interfacing, since the SCL-5424-F watch chip was designed to drive this type of display directly. Again, at this time there was considerable difficulty in



obtaining a liquid-crystal display suitable for a watch. There was quite a lot of literature from various manufacturers, but the only device which was actually obtainable was the LC-201135 from Brown, Boveri and Company. One important advantage gained from using this particular display was its ability to operate from a very low voltage (1.5V to 5V r.m.s.) and still provide a reasonable contrast ratio.

**Crystal.** The quartz crystal required by the SCL-5425-AF is a 32.768 kHz type. Motorola manufacture a suitable crystal in a sub-miniature vacuum envelope — the MTQ-32. They also make a sub-miniature ceramic trimmer capacitor for wristwatches; this is the MTT-02.

**Batteries.** It took the author approximately four months to obtain the main components for the watch, these being logic i.c.s, display, quartz crystal and trimmer capacitor. Batteries were now the only components outstanding on the shopping list and the author confidently expected this to be very easy since he had obtained the "Designers Guide to Battery Systems" from Mallory. This book describes a very comprehensive range of batteries including no less than six specifically designed for electronic watches.

At this time the author discovered that empty wristwatch cases were available from wholesale watchmakers, so rather than try to make one (the die-cast box effect) it was decided to buy a suitable case ready-made. Before this could be done, however, the type and size of battery or batteries would have to be decided upon.

After visiting a number of large jewellers in central London, it was discovered that watch batteries are not available for sale over the counter; electronic watches requiring new batteries are, apparently, returned to the manufacturers to have their batteries replaced.

To have gone ahead and designed a watch using a battery from the Mallory range, but which proved difficult to obtain in practice, would have broken design rule (4). The author spent some time, therefore, visiting chemists,

jewellers and photographic shops in central London to determine which small mercury batteries were easily obtainable. The result of this investigation showed that the best battery for the watch would be the RM-312H mercury battery designed primarily for hearing aids. This is obtainable from most chemists and with a capacity of 36mAh it would appear to fulfil design requirement (4). Three of these batteries are used in the watch and they will have a life in excess of nine months.

**Oscillator design**

The timing reference in this watch is a quartz crystal oscillating at 32.768kHz. This frequency is popular with i.c. manufacturers because it is an exact power of two, ( $2^{15} = 32768$ ) thus simplifying frequency divider design. It is also a compromise between power consumption in the oscillator and the physical size of the crystal; lowering the frequency increases the size of the crystal, making it too large for a wristwatch, while increasing the frequency causes an unacceptable increase in power consumption. Future trends in watch design, however, are tending towards much higher frequencies (as high as 4MHz) to increase stability, with the use of silicon-on-sapphire c.m.o.s. integrated circuits to maintain extremely low power consumption.

The equivalent circuit for the Motorola MTQ-32 quartz crystal is shown in Fig. 1 which gives some typical component values. A typical Q of 50,000 would be obtained. The MTQ-32 is an NT-cut crystal and is mounted in an evacuated sub-miniature envelope.

There are two resonance conditions that a quartz crystal can exhibit – parallel resonance and series resonance. If it is assumed, for simplicity, that  $R_s = 0$ , then the crystal impedance is given by:

$$Z = \frac{j(1 - \omega^2 LC_s)}{\omega^3 LC_s C_p - \omega(C_s + C_p)}$$

The series resonant frequency  $f_s$  is defined at the zero impedance point, where  $\omega^2 LC_s = 1$ , as:

$$f_s = \frac{1}{2\pi\sqrt{LC_s}}$$

The parallel resonant frequency  $f_p$  is defined as occurring at the infinite-impedance point; where  $\omega^3 LC_s C_p = \omega(C_s + C_p)$ , and is

$$f_p = \frac{1}{2\pi\sqrt{L\left\{\frac{1}{C_s} + \frac{1}{C_p}\right\}}}$$

Figs. 2(a) and 2(b) respectively show the variations of  $X_E$  and  $R_E$  with frequency for typical crystal. Unfortunately  $R_s \neq 0$  for practical crystals and the real condition frequencies are called resonance ( $f_r$ ) and antiresonance ( $f_a$ ). These two frequencies are defined as occurring when the crystal appears purely resistive, i.e. when  $X_E = 0$ . In

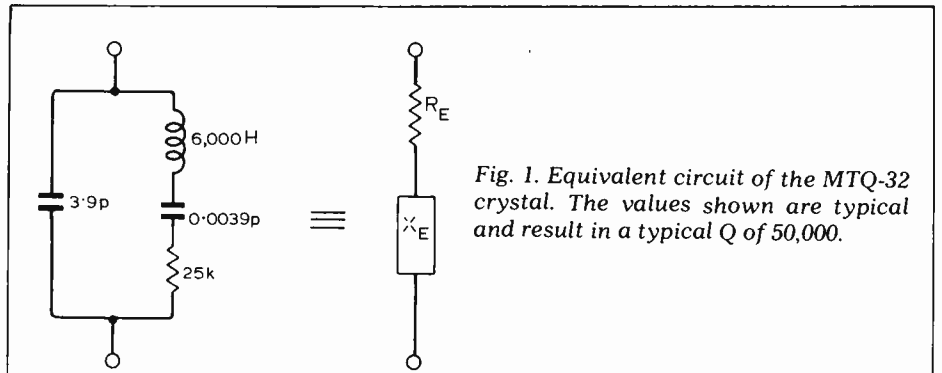


Fig. 1. Equivalent circuit of the MTQ-32 crystal. The values shown are typical and result in a typical Q of 50,000.

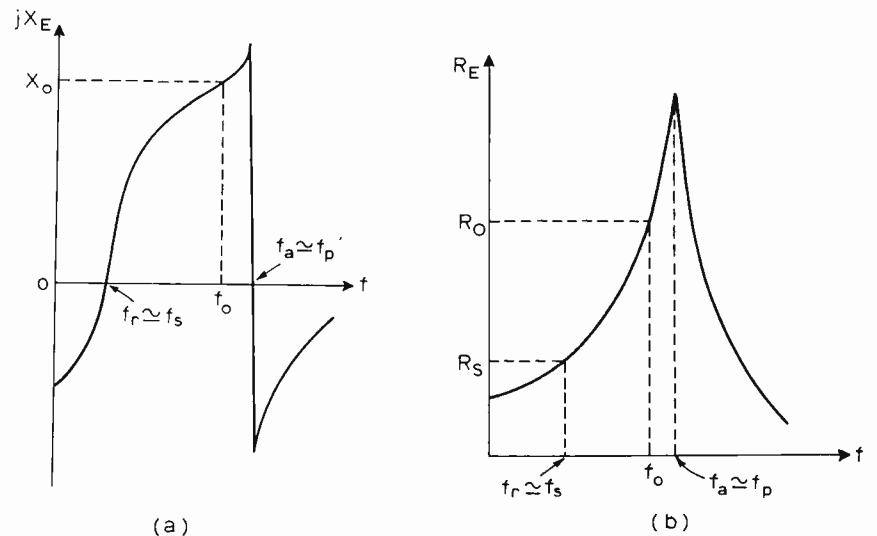
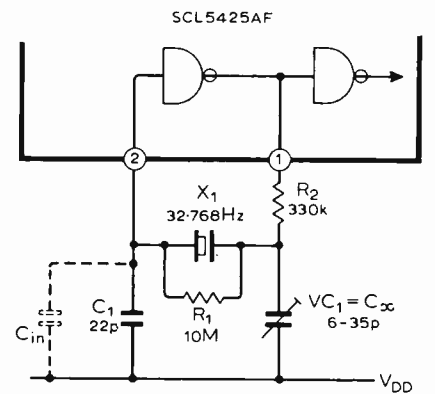


Fig. 2. The crystal reactance  $X_E$  plotted against frequency is shown at (a), while (b) is the resistance  $R_E$  against frequency.

Fig. 3. The practical crystal oscillator circuit, using a logical inverter as the maintaining amplifier. The trimmer is type MTT-02.



practice  $f_r$  is very close to  $f_s$  and  $f_a$  is very close to  $f_p$ . Fig. 3 shows the practical oscillator circuit used in the watch – in this circuit the resonant frequency  $f_0$  lies very close to, but below  $f_a$ . The MTQ-32 crystal is designed to resonate at the specified frequency of 32.768kHz only when it has an external capacitance  $C_L$  of 10-12pF in value in shunt with  $C_p$ .

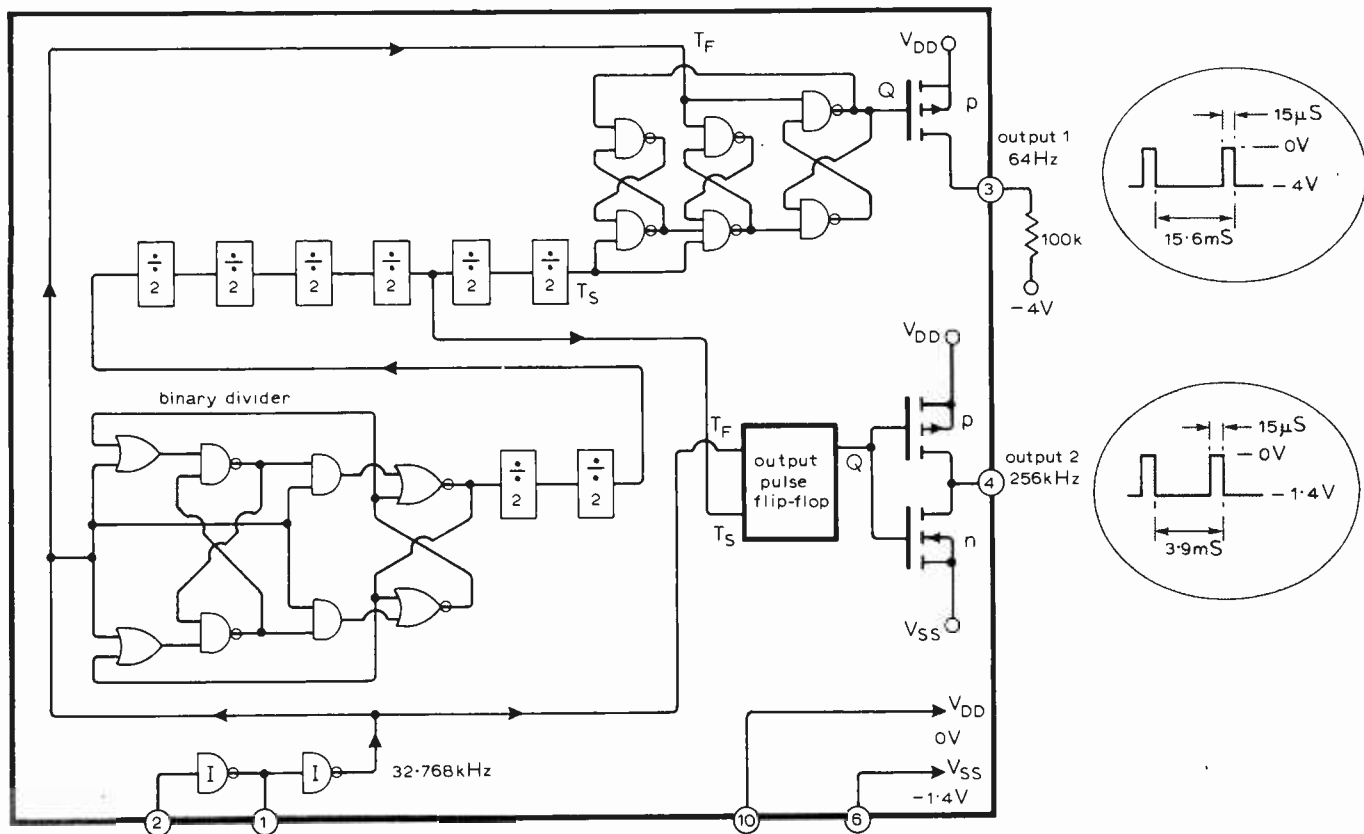
$$C_L = \frac{(C_{in} + C_1)C_x}{C_{in} + C_1 + C_x}$$

where  $C_{in}$  is the input capacitance of the 5425 inverter, and is probably in the region of 5pF.

The inverter is biased into its linear mode by the series combination of ( $R_1 + R_2$ ) which should have a value of about ten times the crystal impedance

at resonance  $f_0$  (typically  $Z \gg 10^6$  ohms) but should be lower than the various d.c. leakage impedances – the inverter input impedance, for example. A value of between 10 and 100MΩ for  $R_1$  satisfies these requirements. Unfortunately, however, physically small high value resistors ( $>10M\Omega$ ) are very scarce; indeed, only a very few types of small resistor can be obtained in values above about 330kΩ. The Mullard CR25 range of carbon film resistors extends to 10MΩ and this is the value of  $R_1$ .

Resistor  $R_2$  controls the drive level to the crystal and contributes to the feedback network attenuation constant. Its value should be about ten times the crystal series resistance  $R_s$ , to give reduced dependence of frequency on the supply voltage.



The trimmer capacitor  $VC_1$  is adjustable between 6 and 35pF, giving a frequency adjustment of about  $\pm 1$  Hz from the nominal 32.768kHz. This represents a timing adjustment of about  $\pm 2\frac{1}{2}$  seconds per day.  $VC_1$  is a sub-miniature ceramic trimmer, the MTT-02, manufactured by Motorola to complement the MTQ-32 crystal.

**Dividers**

The main watch integrated circuit (SCL-5424-F) requires an input of 64Hz and this is provided by the oscillator and divider integrated circuit, the SCL-5425-AF.

Fig. 4 is a logical block diagram of the SCL-5425-AF. It consists of an inverter between pins 1 and 2, to which are connected the frequency determining

Fig. 4. The logic diagram of the SCL-5425-AF.

components to form the oscillator, followed by nine binary dividers. There are two outputs, one at the input frequency divided by  $2^9$  (output 1) and the other at the input frequency divided by  $2^7$  (output 2). With an input of 32.768kHz, output 1 will be  $32768 \div 512 = 64$ Hz and output 2 will be  $32768 \div 128 = 256$ Hz.

The binary dividers used in the 5425 are master/slave toggle flip-flops whose output transitions occur on the rising edge (logic 0 to logic 1 transition) of the

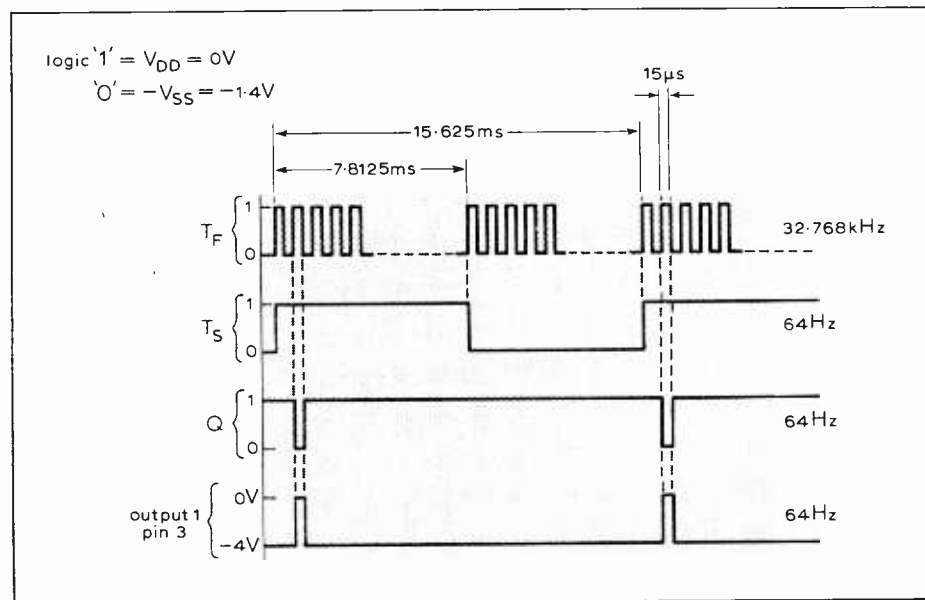
Fig. 5. Generation of low output duty cycles.

input clock. The logical construction of these toggle flip-flops can be seen in Fig. 4. The output from these dividers has, of course, a 50% duty cycle (1:1 mark:space ratio). Resistive loads connected to the outputs would, under these conditions, dissipate an unacceptable amount of power, and the output pulse duty cycle is therefore reduced from 50% to 0.1% for output 1 and to 0.4% for output 2. These low duty cycles are generated by the output pulse flip-flops which are set by the first logic 0 to logic 1 transition of  $T_F$  when  $T_S$  is high and reset by the next logic 1 to logic 0 transition of  $T_F$  (Fig. 5). Further changes in  $T_F$  have no effect until  $T_S$  has gone low and then high again, when another output pulse is generated. The net result of this is that the output pulse flip-flop gates one 15μs pulse of the input frequency at the repetition rate of the output frequency.

Output 1 is an uncommitted p-channel transistor and requires an external drain load of 100kΩ. Output 2 is a conventional c.m.o.s. inverter with an output "on" resistance of 1kΩ at a current of 300μA. This output of 256Hz is primarily intended for driving voltage up-converters to produce the 10 to 15 volts required by many liquid-crystal displays, and it is not used in this design.

**Main logic and display**

A block diagram of the SCL-5424-F watch is shown in Fig. 6. It accepts an input of 64Hz from the oscillator and divider i.c. and directly drives the liquid crystal display. The 64Hz input (pin 23) has an n-channel transistor connected down to  $V_{SS}$  with its gate connected to  $V_{DD}$ . It is intended to provide a load for



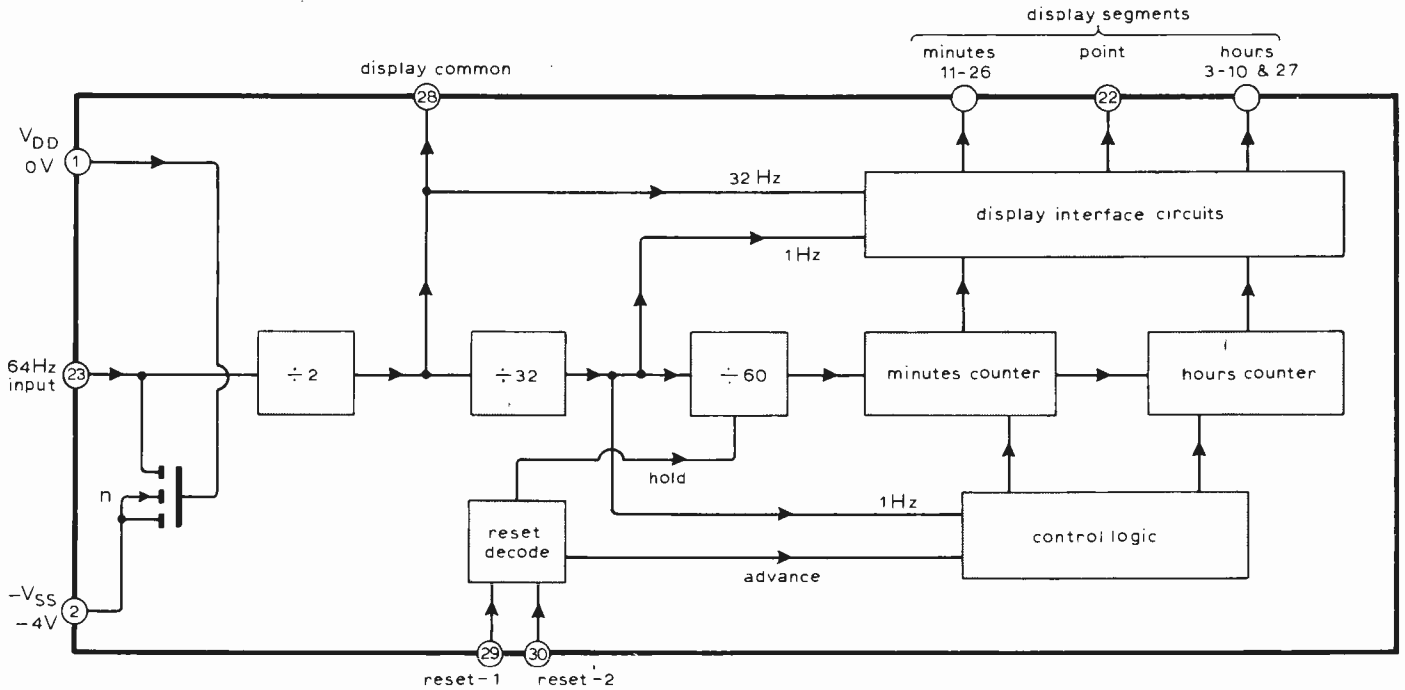


Fig. 6. Block diagram of the SCL-5424-F.

the p-channel current source transistor in the SCL-5425-AF. It is only effective, however, with a supply of 15 volts; with  $V_{ss} = -4$  volts an external resistor of  $100k\Omega$  is required, since at this voltage the transistor has a very high channel resistance. This value of load resistor might appear to be rather low as it results in a peak current of  $40\mu A$  ( $I = 4 \div 10^5 A$ ) but, since there is only one  $15\mu s$  pulse every 15ms (duty cycle 0.1%), the mean current is only  $40nA$ . If this resistor is made too large, then the 64Hz input pulse fall time will be too long and may cause incorrect operation of the divider stages following.

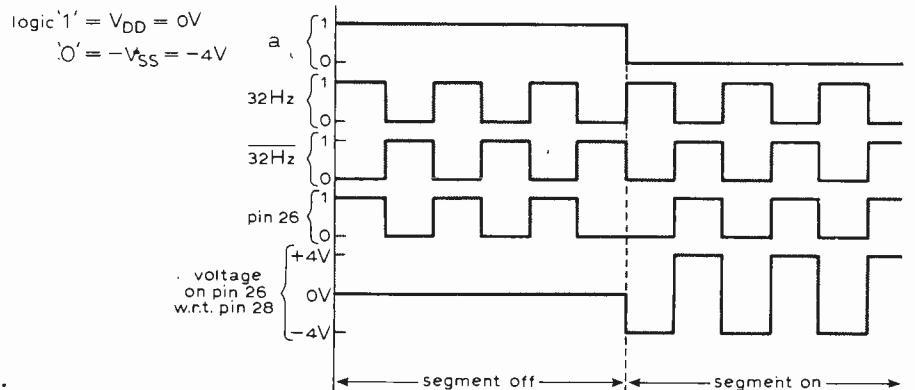
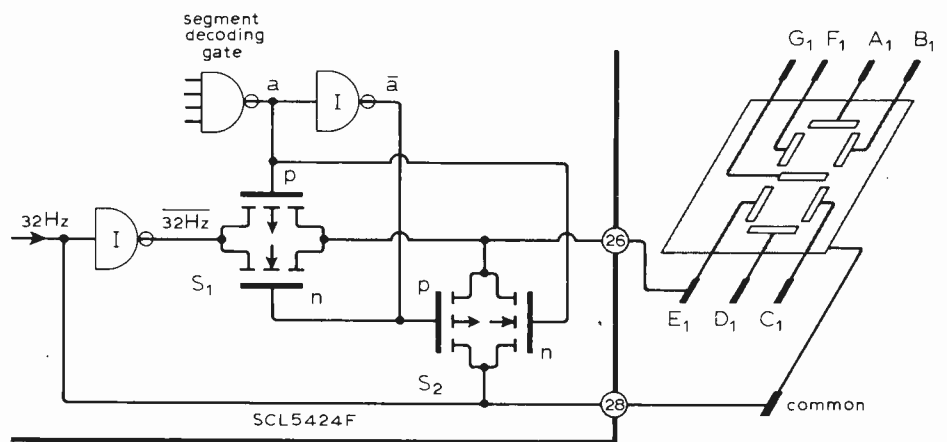
There are two "Reset" inputs (pins 29 and 30) which for normal operation are connected to  $V_{DD}$  (0V) through two  $1M\Omega$  resistors ( $R_4$  and  $R_5$ ). When reset 2 (pin 30) is taken to  $-V_{ss}$  (case potential) the hours increment at a 1Hz rate. Connecting both resets 1 and 2 to  $-V_{ss}$  causes the minutes to increment as for the hours. Connecting reset 1 to  $-V_{ss}$  by itself, stops the watch and resets the divide-by-60 stage preceding the minutes counters. This is to enable the watch to be synchronized to a reference time source, for example, the Greenwich Time Signal.

Liquid crystal displays require a symmetrical a.c. waveform for correct operation. There must be no d.c. component present in this waveform or electrolytic effects within the cell will seriously damage the display, thus shortening its life. The SCL-5424-F watch chip, therefore, contains interface circuitry which produces the required symmetrical square waveform from the output of the seven-segment decoders: Fig. 7 shows one of these circuits together with the associated waveforms. The interface circuit consists, essentially, of two c.m.o.s. transmission gates connected so that the segment output can be either in phase

with the display common output, or  $180^\circ$  out of phase with it.

When all inputs to the segment decoding gate are at logic 1, then its output (a) is logic 0; transmission gate  $S_1$  is on (conducting) and gate  $S_2$  is off. Under these conditions the 32Hz waveforms at pins 28 and 26 are, therefore, out of phase and the net result is that segment  $E_1$  "sees" a symmetrical square wave of 8 volts peak-to-peak, which turns it on. When this segment is

Fig. 7. Display interface circuits.





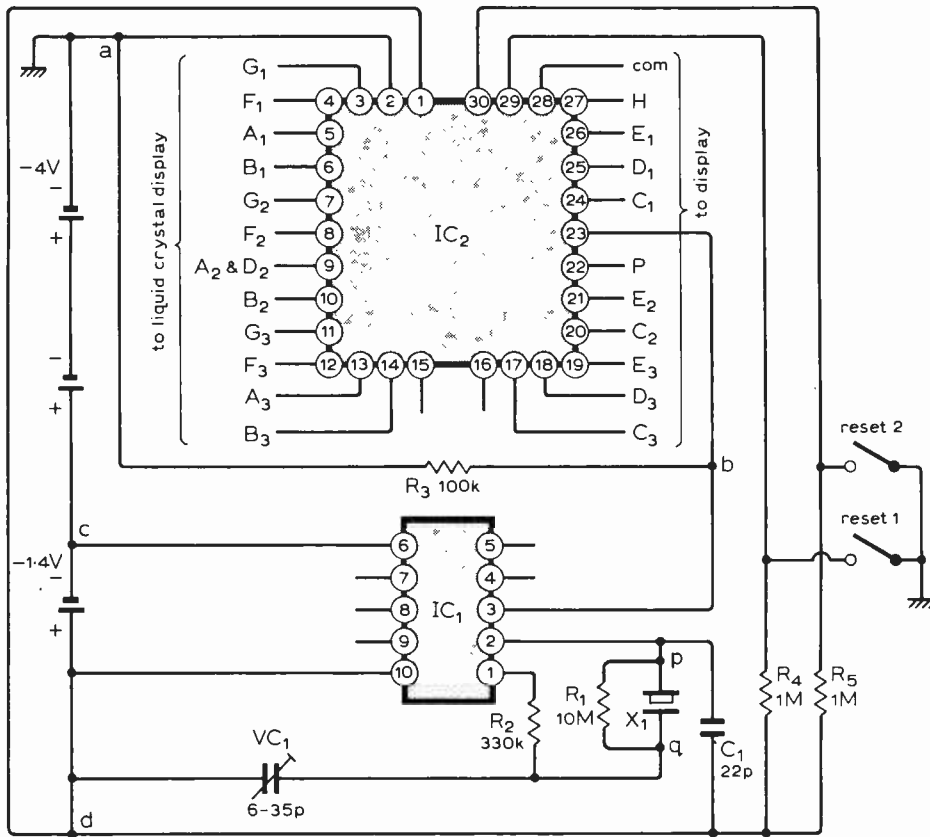


Fig. 8. Complete circuit diagram of the watch.

not required at least one of the inputs to the decoding NAND gate will be at logic 0, its output is logic 1 and transmission gate  $S_1$  will be off, while gate  $S_2$  will be on. There is now no voltage across the cell for this segment, and it is, therefore, off.

Many liquid-crystal displays for wristwatches have a colon between the hours and minutes; the Brown Boveri display used in this design, however, has only a single point. The P output of the watch chip (pin 22) is driven by a 1Hz waveform, through an interface circuit, which results in the display point flashing at a 1Hz rate. This serves two purposes; it gives the wearer confidence that the watch is, in fact, operating, and it can be used as a seconds timer if one is prepared to count the seconds.

**Power supply**

The SCL-5425-AF oscillator and divider i.c., being a silicon-gate device, will operate with a supply voltage between 1.2 and 10 volts: the main logic i.c. (SCL-5424-F), being an aluminium gate device, operates with a supply of between 3 and 15 volts, while the display requires a voltage of between 1.5 and 10 volts: Three 1.4 volt mercury cells, giving a supply of 4.2 volts, satisfy these requirements. The current consumed by the SCL-5425-AF is typically between 2 and  $5\mu A$  at 1.4 volts; above this the current rises quite rapidly, until at 4 volts it will be about  $15\mu A$ . This is far too high for prolonged battery life, so this i.c. is supplied by only one of the three cells. The main logic i.c. and display together consume a maximum current of  $300nA$  ( $0.3\mu A$ ) at 4 volts; the total current required by the complete

watch will, therefore, lie somewhere between  $2.3$  and  $5.3\mu A$ .

The capacity of the RM-312-H mercury cells used in this design is  $36mAH$  or, as it is more usefully quoted in this application,  $4\mu A$ years. These cells will therefore last between nine and about eighteen months. For those constructors who would like to try to obtain one of the range of Mallory watch batteries, the WH1 cell is dimensionally the same as the RM312H but it has a slightly higher capacity of  $45mAH$  ( $5\mu A$ years). (Although the capacity of the RM312H cell is given in the data as  $36mAH$ , this is for a drain of about 2 milliamps and it may in practice have a slightly higher capacity. The capacity of the WH1 is quoted for a current drain of about  $50\mu A$ .)

Fig. 8 shows the circuit diagram of the complete watch, omitting only the display for clarity. (Constructional and operational details will be presented in Part 2 of the article.)

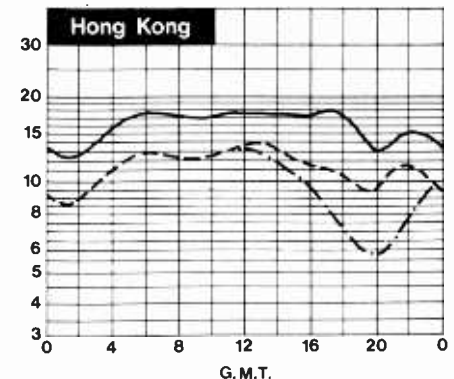
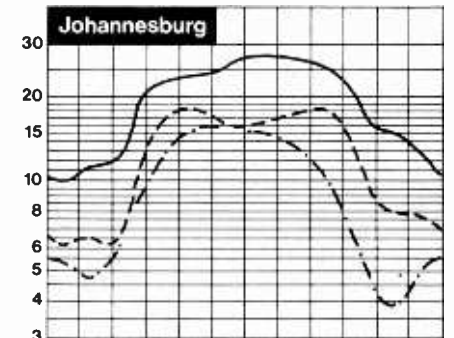
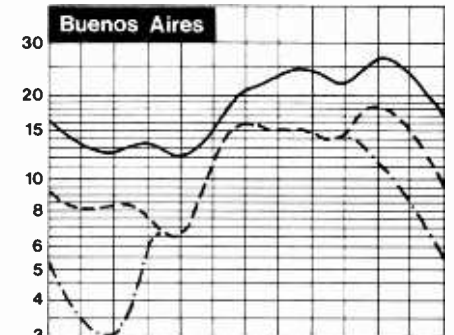
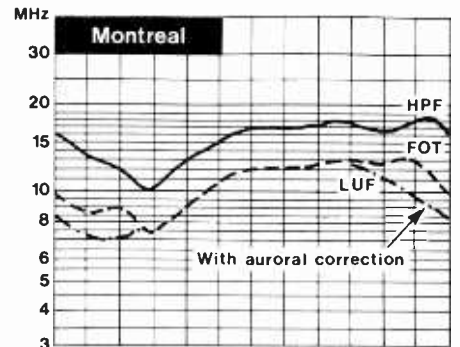
**Vision cassette and cartridge recorders**

Thorn Electrical Industries have asked us to say that the price of the Radio Rentals Contracts Model 8200 V.C.R. is £335 plus v.a.t., or £132 plus v.a.t. per annum when rented. The firm's address is now APEX House, Twickenham Road, Feltham, Middlesex.

**HF predictions**

Magnetic activity is still reaching disturbance level on more than fifty per cent of days. This feature developed rapidly in February 1974 and has persisted to date. The same feature was present in 1973 and terminated abruptly in July of that year.

Smoothed sunspot number is now very low with rate of change near zero. It should start increasing in a few months' time.



# News of the Month

## Josephson faster than transistors

A US patent covering the fabrication of a new type of electronic switch, whose performance far exceeds that of transistors, describes a technique used to grow a thin insulating layer — only 10 to 30 atom layers thick — that is the heart of a device called a Josephson tunnel diode. (The Josephson effect was described in an article by B. D. Josephson in *Wireless World*, October 1966, entitled "New superconducting devices").

It has been recognized for some time that the Josephson effect could provide an extremely fast logic switch that would require very little energy. However, a device based on these effects requires an insulating layer far thinner than has previously been used in electronic devices. The new process, accredited to James H. Greiner of the IBM Thomas J. Watson Research Centre, New York, uses a glow discharge somewhat like that in a fluorescent lamp. When a gas such as oxygen is present in the discharge, an insulating oxide is formed on the surface of the sample up to a certain thickness which is dependent on the oxygen pressure and other factors. As the oxide approaches this thickness, the discharge begins to remove oxide at almost the same rate as it is produced. Thus the oxide layer quickly approaches an equilibrium at the desired thickness.

The Josephson switch device is based on a phenomenon called electron tunnelling. Because electrons appear to behave as waves as well as particles, they can penetrate or "tunnel" through a barrier such as a thin layer of insulation which would be expected to stop them according to classical physics. The type of tunnelling exploited in the new device occurs only at very low temperatures, where some metals lose all resistance to current flow and become "superconductors." It was discovered in the early 1960s that two different types of tunnelling can occur through a thin insulator separating two

superconductors. In one type there is no voltage drop and the insulator acts like a weak superconductor itself. In the other type, there is a slight voltage drop across the insulator. The insulator can be switched from the no voltage drop state by a small magnetic field. (Discovery of these effects was recognised by the 1973 Nobel Prize in physics.)

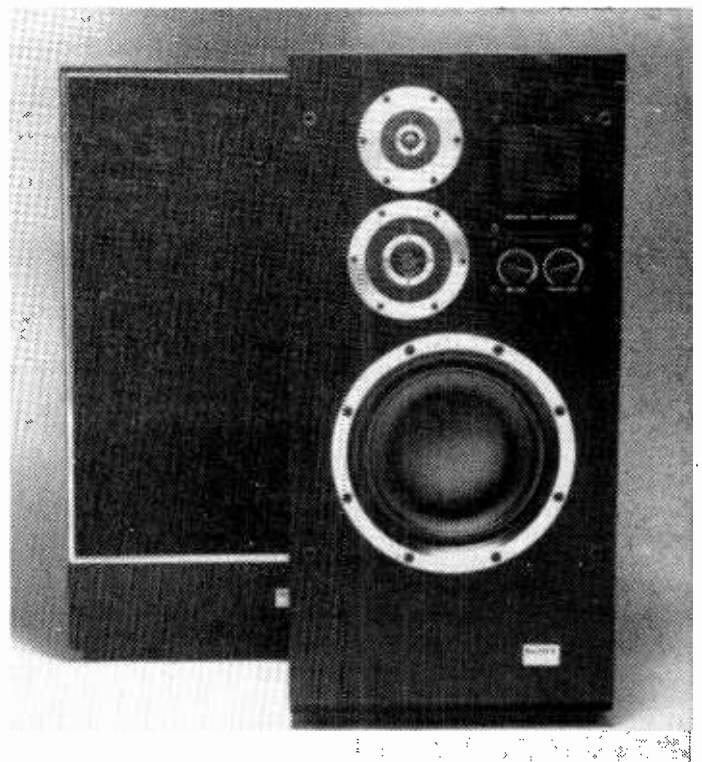
## 1975 Spring trade shows

The annual trade shows for the radio and television industry took place in London during May amid an air of surprising confidence and optimism from both retailers and suppliers. Perhaps also, the fact that this was the last show to be held in the London Hotels before the move next year to the Birmingham exhibition centre was the reason for the unusually large number of exhibitors.

It was very evident, from the range of hi-fi equipment introduced, that many manufacturers believe that one way of ensuring buoyant trade prospects is to move up-market to the very expensive (and very large!) end of the scale. A typical example of this philosophy was to be found at the Cumberland Hotel, where Sony (UK) Ltd were introducing a range of esoteric audio equipment of phenomenally high price. Among these were some loudspeakers priced at about £1,500 a pair and a new reel-to-reel tape recorder priced at around £1,200!

In total contrast, AEG Telefunken were showing some brightly coloured pocket-sized portable radios that were of quite modest price. Significantly, no new developments appeared on show

*The Sony SS8150 loudspeaker is a typical example of a new technique announced during the show. The drive unit cones are loaded with carbon fibre filaments to give a very high stiffness.*



for television, with the exception of an increase in the incidence of slot-mask tubes and the new 20 inch screen size.

Philips were showing a rather battered prototype Teletext decoder incorporated in a large screen television and since it did not seem to be fully functional, little interest was shown by those dealers present at the time.

At the end of the five days, most exhibitors reported a steady trade with dealers buying products, but in many cases, in a cautious way. So much new technology was shown, that this will form the subject of a brief report in the next issue of this journal.

In conclusion, the overall impression gained was of a very high morale and a determination to fight back against the trends of the current decline in consumer sales.

## VAT muddle

The introduction of the 25% VAT rate on certain so-called luxury goods appears to have resulted in a good deal of confusion not only among component suppliers and kit companies but also among advertisers using magazines such as *Wireless World* which are aimed at a combined audience of professional engineers and enthusiasts.

As a result we have asked the Customs and Excise for clarification on a number of common questions. The question of VAT liability requires that a distinction be made between those who are VAT registered and those who are not.

For those who are registered, VAT is recoverable, so no change will result in accounting procedures. The changes affect the non-registered purchaser who

is either a business with a turn-over less than £5,000 per annum, or is a private purchaser. The types of goods and services subject to the high rate of VAT are defined in Notice 742 from Customs and Excise and are quite clear in all instances except where related to components and borderline products having a possible consumer application.

Taking components first; all those components forming parts of higher rated goods are subject to 25% VAT. Those that have been specifically excluded by the VAT Liability Office may be rated at the higher rate, if they are fitted as a spare part by an engineer performing a service classified at the higher rate. Examples of such components would be those that are rated to a higher specification than that normally used in, say, audio amplifiers. Hence a high power thyristor is excluded and rated at 8% unless it is used by a service engineer as a spare part in a domestic audio amplifier.

A telephone enquiry to the VAT Liability Office elicited the information that there are still many "grey" areas where final decisions on rating have yet to be made. They informed us that local VAT offices are issuing conflicting information and that enquiries concerning electronic and electrical goods not specifically mentioned in Notice 742 should be addressed via the appropriate trade association who will then negotiate with the London VAT Liability Office. It is only this office that is in the position of making final decisions on specific exclusions.

The VAT officer went on to say that in the intervening period of uncertainty, manufacturers are expected to make their own decisions regarding the rating of their components, in instances where Notice 742 has provided insufficient information.

Finally, two specific examples of liability in relation to advertising. Notice 742 states "Appliances . . . are generally regarded as being for domestic use if they are . . . advertised in those periodicals intended for the public." We are informed by the VAT Liability Office that this is only one of the criteria applied and that where the only advertising outlet for a professional product is through a publicly available journal than this would not result in the high rate being applied. For example, public address equipment is tentatively rated at 8% (subject to discussion with the trade associations resulting in a permanent decision). Advertising in a magazine such as *Wireless World* would not result in the high rate being applied. Similarly professional discotheque equipment may be advertised in the *Melody Maker* and yet be rated at 8%.

All this note serves to show is that in areas of doubt final clarification can only be obtained from the central VAT Liability Office, preferably through a trade association.

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## Antenna system for AEROSAT

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A complete L-band aircraft antenna system of a type suitable for airliners using the projected AEROSAT aircraft/satellite communication system has been developed under contract to the Ministry of Defence in close co-operation with the Royal Aircraft Establishment and completed in time to be installed in one of RAE's Comet 4 aircraft for the AEROSAT system trials. The trials, based on the Azores, are organised by the European Space Research Organisation and started at the end of February. NASA's ATS6 satellite is being used to assess performance of the L-band system, which is of particular significance since in this geographical area the access angle from the aircraft to the satellite is low, resulting in appreciable noise temperature and accentuating possible multipath problems.

The antenna system consists of two antenna groups with two switching and phasing units with their associated cabling. The antenna groups are virtually flush mounted on each side of the aircraft fuselage at about 40° from the zenith. The switch units are installed in a convenient location inside the fuselage.

An antenna group consists of six slot-dipole elements, three transmitting and three receiving which give the required beam coverage with good multipath signal rejection. The slot-

dipole element itself was developed by RAE's Radio and Navigation Department and was selected after detailed examination of a wide range of alternative elements. The L-band system is rated at 200 watts, 50% duty, and has been designed to transmit on 1640-1660MHz and receive on 1540-1560MHz with omni azimuth coverage for elevation angles of 10° and above. After two weeks and nearly 50 hours of flying time the antenna system was working well. There were several days of torrential rain when the Comet 4 remained on the tarmac, during which time the impedance of both the transmitter and receiver were measured several times and no change was observed.

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## Brema on VAT

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The following text of a telegram to Members of Parliament was issued by the British Radio Equipment Manufacturers' Association on 22nd April. "To all members of Parliament from Lord Thorneycroft. President of British Radio Equipment Manufacturers' Association. The recent budgetary proposals to increase VAT to 25 per cent will have the immediate effect of causing serious and permanent redundancies in this industry. At a special meeting of the Association today member companies estimate that permanent and unavoidable lay-offs of staff would exceed 6,000 at least 20 per cent of direct labour employed by the industry. These figures in addition to the 5,000 redundancies which occurred in the calendar year 1974, and exclude serious position which will undoubtedly occur in component and associated industries. Position is grossly aggravated by the retro-active effect of VAT proposals on rental side of industry. We wholeheartedly endorse representations already made by members of the National Television Rental Association. We emphasise that enforced reduction in production capacity now cannot fail to increase the cost of imports when the market next improves, with serious consequences on balance of payments position."

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*"No madam, this is not Harrods." Pyc Telecommunication's specially adapted "Westminster" mobile radiotelephone in use at the Silverstone Racetrack during recent police trials. The police motorcyclist is using the hand-set for transmitting, and a loudspeaker, mounted on the motorcycle's fairing, for receiving.*




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## Is circularly polarized TV coming?

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The heading to this item was the title of a paper by M. S. Siukola presented in the *IEEE Transactions on Broadcasting*, Vol. BC-21, No. 1, March 1975. According to the paper, there is on the horizon a new approach to the way TV signals are radiated. The technique is circular polarization, and while this has been in use for several years in f.m. broadcasting, it is now being viewed for TV as an

effective antidote for ghosting, spotty coverage, multipath, poor reception on whips and rabbit ears, misoriented antennas, co-channel and adjacent-channel interference – all ills that have plagued broadcasters and viewers since TV's inception. The conclusions reached in the paper indicate that the principal deterrent would seem to be the cost to the broadcaster, but this may well be completely compensated by the more solid coverage, increased viewer enthusiasm for the enhanced reception and the additional viewer audience that circularly polarized TV is expected to provide within existing coverage areas. Present receiving antennas would not be made obsolescent, but viewers would certainly benefit most by acquiring circularly polarized types. The designs for receiving antennas as well as transmitting types are available and the antennas can be built now.

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## Association of research contractors formed

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The Association of Independent Contract Research Organizations has been formed to represent and promote the resources of seven constituent founder members. Contract research is becoming increasingly important in its scope for serving industrial, commercial, institutional and governmental clients as a world-wide business. The seven major independent organizations based in the UK serve home and overseas markets. Between them they employ 2,250 staff of whom 800 are of professional consultant status. The Association aims to communicate on behalf of its members with international and intergovernmental bodies, with central governments in the UK and overseas, with industry – representational bodies and industry groups – and with commercial organizations able to benefit from contract research services. Further information can be obtained from D. McA. Craig, 7 Catherine Place, London SW1E 6EB.

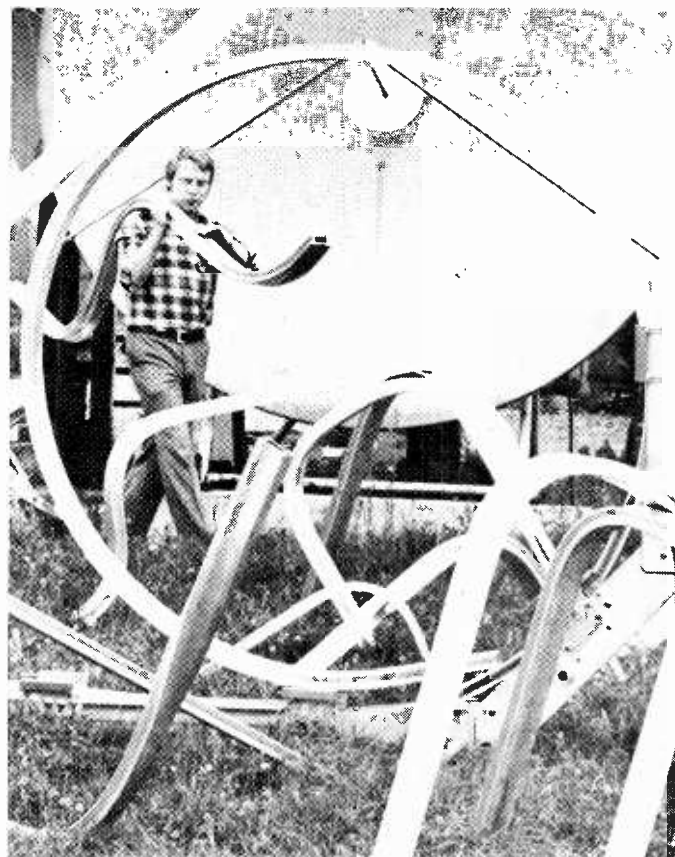
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## Queen's awards to electronics

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Worthy of note are the following companies who were included in those honoured by the Queen earlier this year for their contribution to Britain's technological development and exports: Beckman Instruments for export achievements during the last three years; Mullard for outstanding export success and development; Micro Consultants for outstanding work in the field of ultra high speed analogue-to-digital conversion; EMI Sound and Vision Equipment for export achievement of the brain diagnostic EMI-Scanner;

*For radio relay systems using the microwave range above 3GHz Siemens are now developing aluminium waveguides with rectangular cross sections which can be bent and twisted and which simplify the planning and installation of connecting lines between radio relay equipment and antennas.*



Marconi-Elliott Avionic Systems for technological innovations in the sophisticated navigation and weapon aiming system NAVWASS, supplied for Jaguar aircraft; KEF Electronics for export achievement of loudspeakers; Sinclair Radionics for outstanding export achievement and for technological innovation in electronic calculators; British Aircraft Corporation for export achievement and for technical innovation in high performance flight radomes by the Reinforced and Microwave Plastics Group. Our congratulations go to all concerned.

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## Transistor assembly automated

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A recently developed transistor assembly system that can assemble a variety of transistor types by means of pattern recognition techniques comprises a minicomputer and image processors and will ultimately have 50 wire-bonding machines with visual functions to determine chip positions of transistors fed into the machines. The system has been installed at Hitachi's Takasaki Works, in Japan.

To recognise the position of transistor chips, an artificial eye is needed to replace the human eye. For this purpose, a microscope and a TV camera are mounted on each wire-bonding machine, so that the image signal from the camera is analyzed by a combination of the image processor and the computer to give a high-speed position

recognition rate of 0.2 seconds per chip average. Position data is fed back from the computer to the appropriate wire-bonding machine, whose servomechanism can stretch the gold wire between emitter and base electrodes on the chip and the corresponding outer leads. It is claimed that the production rate has more than doubled since replacement of traditional methods.

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## World markets decline

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An extract from the 1975 first quarter and stockholders meeting report issued by Texas Instruments indicated that the decline in demand for their electronics products experienced in 1974 was generated by the longest, deepest recession since recovery from World War II. The major difference between this and past recessions is the almost concurrent decline of all major economies. In 1970, while the US economy was declining, Japan and Europe continued to grow. In contrast, late 1973 industrial production turned down simultaneously in Japan, Europe and the US.

In the US real growth has dropped for the past five quarters. High unemployment, inventory liquidation and sluggish capital spending suggest they (TI) will not reach the bottom before the third quarter of 1975, with at best a modest upturn this year and a slow recovery in 1976.

Japan appears close to the bottom of its recession, spring wage negotiations



influencing the rate of recovery. West Germany probably will have a moderate upturn in the second half of the year. France will have minimal real growth in 1975. In Italy, industrial production is falling still, but the trade balance is improving and inflation is down compared with 1974. The UK economy is expected to remain sluggish well into 1976.

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## Direct-drive a.c. motor

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Matsushita, who are represented in the UK by Symot, have announced a direct drive a.c. motor for use in record turntables. The unit, which is called the FF-2000 is basically a linear motor, which drives a light-weight aluminium platter, by eddy currents. Underneath the platter is a geared magnetic speed sensor which forms part of a feedback system for speed regulation. The motor is electronically controlled and requires an a.c. supply of 18V, 40mA. Performance of the FF-2000 is claimed to be equal to or better than the existing d.c. direct-drive motors used in the Technics range (also manufactured by Matsushita). We understand that these motors will cost around £12. in production quantities, and will be available at the end of this year.

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## Ceefax, Oracle — now Tifax

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Texas Instruments announced at a press conference given in May that they have now completed the design of a modular data processor which will decode the Teletext transmissions broadcast by the BBC and IBA. Although no product has yet appeared, samples of the first generation processor will become available later this year, followed by full production in 1976.

What makes the difference in the "Tifax" decoder, from those already designed by such companies as Decca and GEC, is that the Tifax unit is being offered as a p.c.b. module carrying a relatively small number of dedicated l.s.i. circuits.

The projected cost of the "Tifax" module is expected to be around £50, reducing to £10-£15 over a few years. Power consumption is said to be 5W drawn from a regulated +5V  $\pm$ 0.25V supply with a maximum ripple of 10mV pk-pk. Interface to the receiver is by direct connection to the R.G.B. video drive stage from 15V, 20mA current sink open collector outputs. The brightness display can be varied using three integral common base transistors. The video input requires a signal amplitude of 2-3V pk-pk, negative going sync, with an input impedance of typically 10k $\Omega$ .



*New microwave distance measuring equipment, the Tellurometer MRA5, indicates directly in metres and centimetres, operation being either fully automatic or manual at the choice of the operator. Measurement can be accomplished in less than 20 seconds.*

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## Microwave Conference overwhelmed

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The organizers of the fifth European Microwave Conference, which takes place September 1-4, 1975, at the Congress Centrum, Hamburg, have announced the list of papers that have been selected by their technical programme Committee and paper review board for this annual event. The response to the conference call for papers has been overwhelming. Over 350 papers from 30 countries were submitted and from those, a total of 112 will be presented at Hamburg. The papers will be grouped into 20 sessions and the morning sessions will be preceded by a total of nine specially invited state-of-the-art survey papers to be given by a number of the world's leading microwave experts. Papers will be presented in English and are limited to 15 minutes duration. A book of abstracts for the conference was published during May. Further information can be obtained from the organizers, Microwave Exhibitions and Publishers Ltd, Temple House, 34-36 High Street, Sevenoaks, Kent TN13 1JG.

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## TV deliveries down again

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Deliveries to UK distributors of UK-made and imported colour television receivers reached 139,000 in March, a 26% decrease over March 1974 (188,000), according to the latest statistics compiled by the British Radio Equip-

ment Manufacturers' Association. This brought the year's total to 475,000, a fall of 23% compared with the same period in 1974 (619,000). Total monochrome television deliveries for March were 63,000, a fall of 22% compared with March 1974. BREMA members delivered 65,000 audio stereo systems in the month, a fall of 10% compared with March 1974 (72,000). This brought the year's total to 192,000, comparable with 202,000 for the same period in 1974. Deliveries of radio receivers reached 351,000 for the month, bringing the year's total to 1,032,000, compared with 1,345,000 in 1974, a fall of 23%.

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## Briefly

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**IEA plus Electrex.** The International Instruments, Electronics and Automation Exhibition running at Olympia since 1957 and the International Electrical Exhibition (Electrex) organised at Earls Court since 1953 are to be held as a combined event, short title IEA-Electrex, in 1976, at the new National Exhibition Centre, Birmingham.

**VAT late extra.** An itemized list of components on which specific agreement has been reached between HM Customs & Excise and the Electronic Components Board is now available. It is recognized that there may be some individual products to which the application of these definitions is not entirely straightforward. In such cases, an individual ruling will be given by Customs & Excise, the facts being initially reported to the Electronic Components Board.

## Teletext

We plan to publish in the near future a short series of articles on the Teletext television information system, culminating in a design for a decoder for use with domestic receivers. Teletext is a unified version of the BBC's CEEFAX system (*Wireless World*, May 1973, p.222) and the ORACLE system developed by the IBA (July 1973 issue, p.314). Test transmissions were started by the BBC in September 1974 on BBC1, while a group of independent television companies (London Weekend, ITN and Thames) will be starting them in July 1975. The Teletext broadcasting standard was outlined in News of the Month, November 1974 issue.

# Active notch filters

## Design theory behind the development of discrete frequency rejection circuits

by Yishay Nezer, B.Sc.

**We often need to separate a wanted signal from periodic interference. This may happen, for example, when a whistle or a power-line hum is disturbing a radio programme. In simple cases a filter which has zero transmission at one discrete frequency and unity transmission at all other frequencies is sufficient. In contrast to a practical low-pass or high-pass filter, an almost ideal notch filter can be realized with only one section; moreover it can be voltage tuned or even automatically track the interference.**

The major class of notch filters, both passive and active, is of the second order and has the following transfer function:

$$G(s) = \frac{s^2 + \omega_0^2}{s^2 + \frac{\omega_0}{Q_0}s + \omega_0^2} \quad (1)$$

where  $\omega_0$  is the rejection frequency and  $Q_0$  is the figure of merit of the filter, which is given by  $Q_0 = \frac{\omega_0}{\Delta\omega}$  where  $\Delta\omega$  is the rejection bandwidth defined by the 3dB attenuation points. Some typical frequency response curves are plotted in Fig. 1 with  $Q_0$  as the fixed parameter.

Many passive notch networks are known. This article will deal mainly with RC networks, since the use of coils is inconvenient, particularly at low frequencies. The best-known RC notch network is the symmetric twin-tee illustrated in Fig. 2(a), for this network  $\omega_0 = 1/RC$  and  $Q_0 = 1/4$ . The function is, of course, realized only if the network is fed by a voltage source and subjected to an infinite load.

Another well-known notch network is the Wien bridge. This network is characterized by  $\omega_0 = 1/RC$  and  $Q_0 = 1/3$ . The left side of the bridge shown in Fig. 2(b) is composed of equal resistors and capacitors and, in order to obtain an infinite null, the other two resistors must satisfy the relationship  $r_1 = 2r_2$ . The notch response, however, can be achieved even if the corresponding components in the reactive side of the bridge are not equal. The rejection frequency will then be  $\omega_0 = 1/\sqrt{R_1R_2C_1C_2}$  but the ratio  $r_1/r_2$  will no longer equal two. An important special case occurs when  $R_1 = 2R_2$  and  $C_1 = C_2/2$ ; we then have  $r_1 = r_2$ .

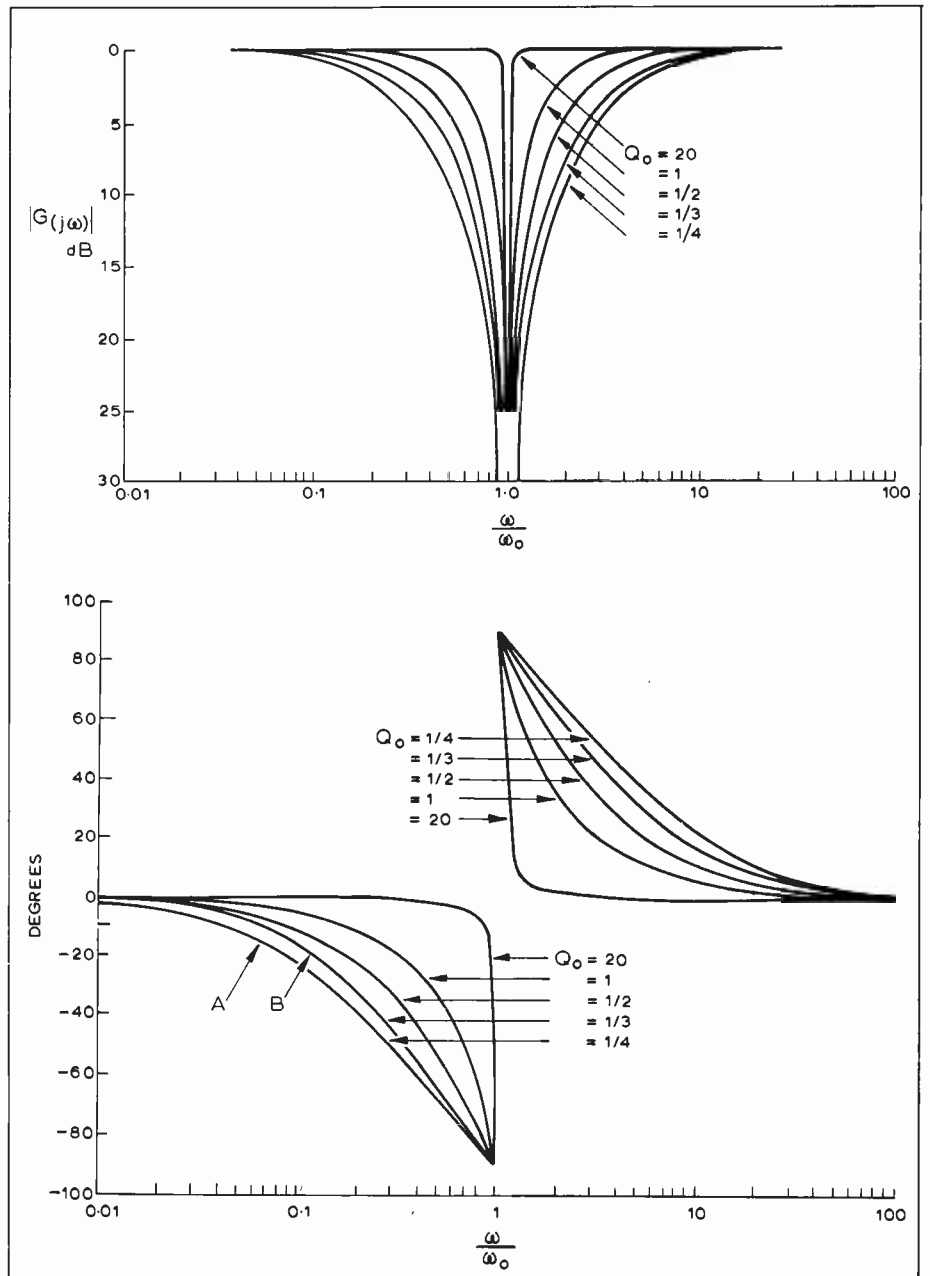


Fig. 1. Normalized phase and magnitude response curves of a notch filter for several values of  $Q_0$ .

A drawback of the above two networks is that in order to vary the centre frequency and still maintain the infinite null, two or three closely matching ganged variable components must be used. Several RC bridge networks are known in which a single component is sufficient to control the rejection frequency. However, their practical significance is limited because the frequency response becomes severely asymmetric as the rejection frequency is varied.

A more acceptable variable network was proposed by Hall<sup>1</sup>. It is shown in Fig. 2(c). This network can be tuned by means of a single potentiometer and the tuning law is  $\omega_0 = 1/RC\sqrt{\alpha(1-\alpha)}$  which in theory spans the whole frequency range. In practice the tuning range is quite limited due to the extreme non-linear dependence of  $\omega_0$  on  $\alpha$ . However, this network has unity gain on both sides of the null frequency, irrespective of the tuning.

However, unlike the twin-tee and the Wien bridge it is asymmetric on a logarithmic frequency scale. This follows from the fact that the transfer function of this network is not given by expression (1) but contains an additional real pole and real zero.

A similar potentiometer tuned null network based on the twin-tee was proposed by Andreyev<sup>2</sup>.

All the networks discussed so far are

characterized by low selectivity. In fact<sup>3</sup>, no passive RC notch network, however complex, is capable of achieving  $Q_0$  higher than 0.9. If the notch filter must be passive, a relatively high  $Q_0$  may be achieved by including an inductance as in the bridged-tee network shown in Fig. 3. In order to achieve a complete null this network must satisfy the two conditions:

$$\begin{aligned} \omega_0^2 &= C_1 + C_2/LC_1C_2 \text{ and} \\ \omega_0^2 &= 1/rRC_1C_2 \end{aligned} \quad (2)$$

The figure of merit will then be  $Q_0 = 2\omega_0L/r$ , i.e. proportional to the quality factor of the coil.

**Active notch filters**

As has been mentioned above, passive RC notch filters suffer from a low selectivity. A theoretically unlimited selectivity can be obtained by the use of active notch filters. These can be built by various active realizations of the transfer function given by expression (1). Simple active circuits are based on passive null networks in which the selectivity is raised by means of negative feedback.

One such scheme is shown in Fig. 4 and the effect of feedback can be explained as follows: When the feedback loop is open the network is simply a passive null network with a passband gain of  $A_0$  represented by curve (a) in Fig. 5. When the feedback loop is closed,

the network tends to maintain a voltage gain of  $A_0/(1 + A_0)$ . However, it fails to do so where the forward gain is low, i.e. in the vicinity of  $\omega_0$ . As a result, the response curve is compressed as shown in curve (b) and the rejection band is narrower. As an additional benefit, the active filter can now be cascaded without being subjected to loading.

The calculated transfer function of the active notch filter is:

$$G(s) = \frac{A_0}{1 + A_0} \cdot \frac{s^2 + \omega_0^2}{s^2 + \omega_0s/(1 + A_0)Q_0 + \omega_0^2} \quad (3)$$

A different realization is shown in Fig. 6 which relies on a single, less-than-unity gain amplifier. It can be seen that there are two feedback paths in the configuration, a positive unity-gain feedback which renders the effective gain of the amplifier equal to  $K/(1-K)$  instead of  $K$ , and a negative feedback which subtracts the output voltage from the input. If  $K/(1-K) = A_0$ , this method is equivalent to the former and the transfer function is:

$$G(s) = \frac{s^2 + \omega_0^2}{s^2 + \omega_0s(1-K)/Q_0 + \omega_0^2} \quad (4)$$

in which the selectivity is multiplied by  $1/(1-K)$ .

**Practical circuits**

The simplest amplifier for the above method is the emitter follower. How-

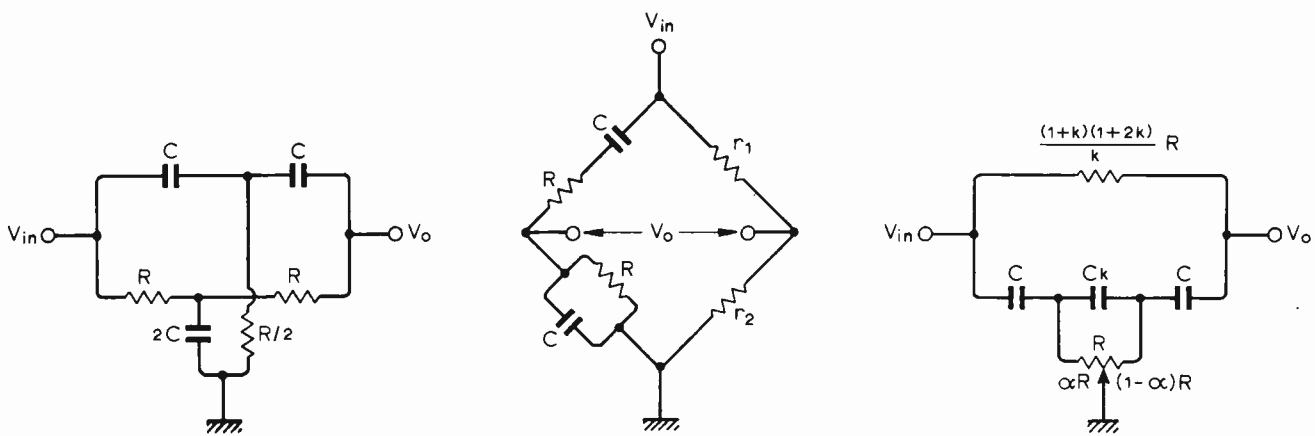


Fig. 2. Three RC null networks: (a) the symmetric twin-tee, (b) the Wien bridge, (c) a potentiometer-tuned network.

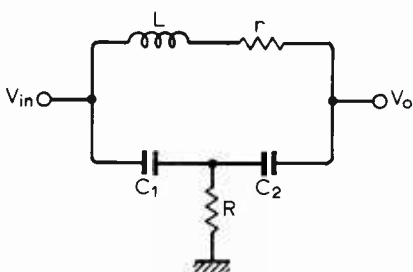


Fig. 3. Bridge-tee RCL null network, the selectivity of which depends on the Q factor of the coil.

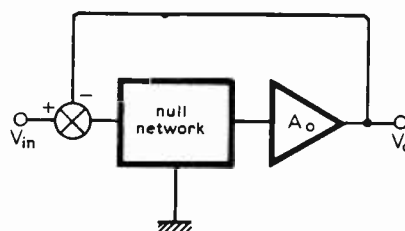


Fig. 4. Basic active configuration for enhancing the selectivity of passive notch filters.

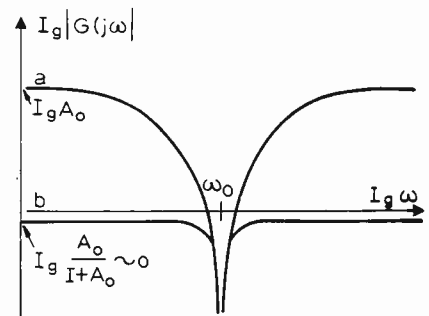


Fig. 5. Frequency characteristics of the network in Fig. 4 (a) open loop, (b) closed loop.

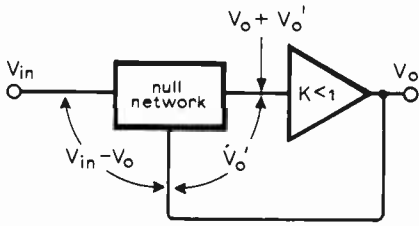


Fig. 6. Practical configuration for enhancing the selectivity of a passive notch network with a single voltage amplifier having a gain of less than unity.

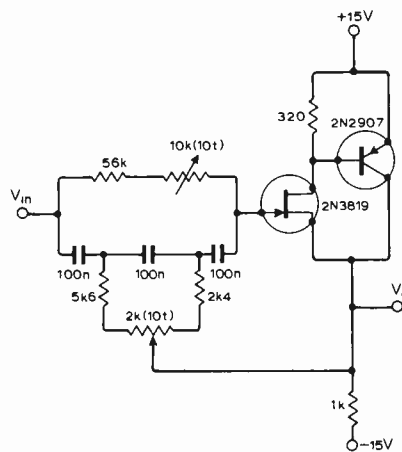
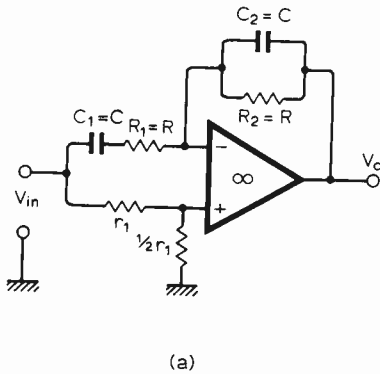
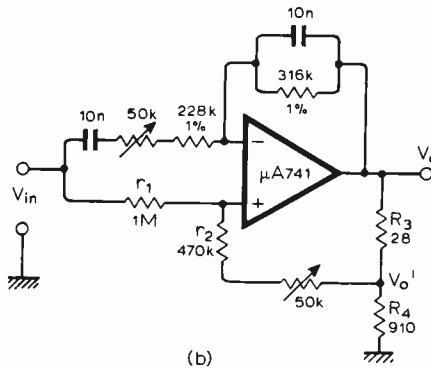


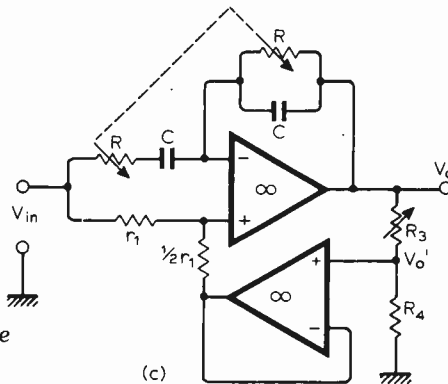
Fig. 7. Simple potentiometer-tuned active notch filter based on the network in Fig. 2(c). Tuning range  $200 \pm 10\text{Hz}$ ; rejection bandwidth  $10\text{Hz}$  (3dB).



(a)



(b)



(c)

Fig. 8. (a) Wien bridge converted to a three-terminal network; (b) 50Hz active notch filter; (c) variable rejection frequency and bandwidth Wien-bridge active notch filter.

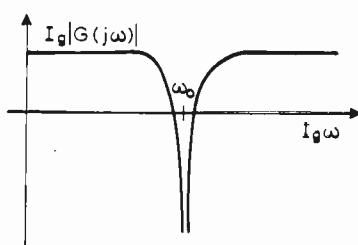


Fig. 9. Wider rejection bandwidth is attained by cascading two notch filters.

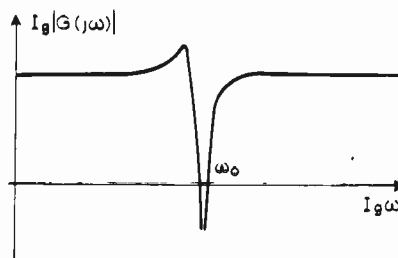


Fig. 10. Asymmetry in the frequency response curve of high Q notch filter as a result of excessive phase shift in the amplifier.

ever, it is not very suitable because in order to prevent the null network from being loaded by the relatively low-input impedance, the resistors must be relatively low and the capacitors must be correspondingly large.

It is obviously possible to replace the transistor by an f.e.t. and use smaller capacitors, but the increase in the selectivity would be limited due to the smaller gain usually associated with the f.e.t. The bootstrapped source follower benefits from high-input impedance and also a gain closer to unity and is shown in Fig. 7 together with the network of Fig. 2(c).

The networks discussed above have ideally an infinite attenuation at the notch frequency. Practically, the attenuation is limited by the tolerances of the components and is typically 40dB for 1% tolerance. This figure may be exceeded by trimming and is ultimately limited by stray capacitance.

The Wien bridge is attractive owing to its simplicity. However, it is not a three-terminal network, and cannot be activated directly.

The circuit in Fig. 8(a) is a Wien bridge built around an operational amplifier. In spite of being active, the factor of merit is only  $\frac{1}{2}$  instead of  $\frac{1}{3}$  in the passive bridge (it does not belong to either of the schemes shown in Figs. 4 and 6) yet, being a three-terminal network, its selectivity can be improved as shown in Fig. 6. Since the output impedance is already zero an additional buffer amplifier is unnecessary, so that we only have to decrease the gain to below unity by a voltage divider and close the feedback loop at  $r_2$ . The network Fig. 8(b) then contains an equivalent amplifier whose gain and output impedance are:

$K = R_4 / (R_3 + R_4)$  and  $R_3 \parallel R_4$  respectively. Accordingly, the latter value must be subtracted from  $r_2$  or must be much smaller. Alternatively the voltage divider can be buffered as in Fig. 8(c).

If we use  $V_o$  as the output of the filter instead of  $V_o'$ , an advantage results with respect to the network of Fig. 6, in that the passband gain is unity instead of  $K$ . However, as the internal amplifier's gain is  $K = R_4 / R_3 \times R_4$ , the factor of merit will be

$$Q = Q_0 / (1 - K) = (1 + R_4 / R_3) / 2 \quad (5)$$

and the rejection bandwidth can be varied by means of either  $R_3$  or  $R_4$ . The null frequency can be varied, for example, by  $R_1$  and the notch depth can then be adjusted by means of  $r_2$ .

If it is desired to vary the rejection frequency over a wide range, it is best to vary simultaneously resistors  $R_1$  and  $R_2$ . If the tracking is good, the null will be maintained throughout the tuning range without further adjustments.

### High Q notch filters

At a frequency  $\omega = \omega_0(1 \pm \epsilon)$  close to the resonant frequency, that is  $\epsilon \ll 1/2Q$ , the response of a notch filter can be approximated by two



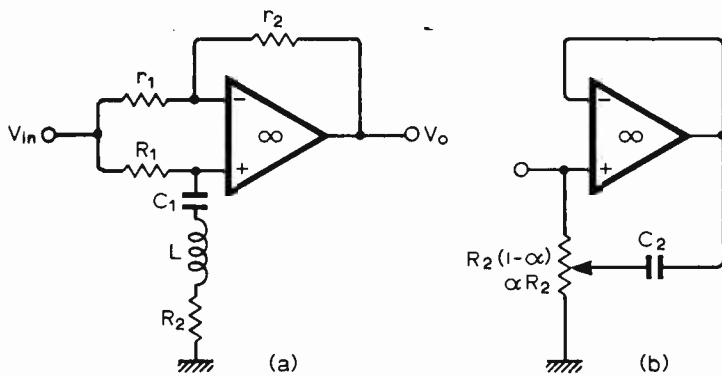
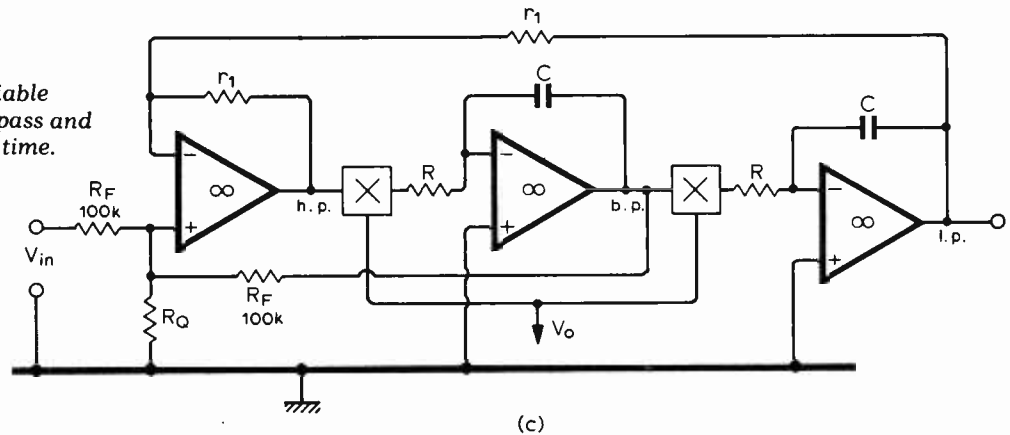


Fig. 11. (a) An active RCL notch filter; (b) a potentiometer-controlled simulated grounded coil.

Fig. 12. Programmed state variable filter provides low-pass, band-pass and high-pass outputs at the same time.



straight lines with slopes  $\pm 2Q$ , and the filter can be used as a frequency discriminator. If  $Q$  is large, very small frequency deviations can be observed. On the other hand, if a high  $Q$  notch filter is used to reject a power-line hum, for example, a slight deviation of the frequency from its nominal value will suffice to render the attenuation excessively low. In this case a filter with an infinite attenuation over a band of frequencies would be desirable. However, such a filter cannot be realized. It is then possible either to lower the  $Q$  of the filter or to stagger-tune two or more filters in cascade and obtain a frequency response as in Fig. 9. A more elaborate solution is to use an interference tracking notch filter as suggested in the last paragraph.

When dealing with high  $Q$  notch filters, the increasing sensitivity of the notch symmetry and depth to the tolerance of the passive components becomes a serious problem. A practical solution is to use stable capacitors and trim resistors for the required notch frequency and depth. It has been seen that the most suitable network from this standpoint is the Wien bridge, but for ultimate stability the state variable filter (see below) is required owing to its extreme stability.

Another problem in realizing high  $Q$  notch filters is the roll-off in the open loop gain of operational amplifiers at high frequencies. It is found that there is a limitation on the maximum possible  $Q$  which is inversely proportional to the rejection frequency. This limitation may cause asymmetric frequency

response (Fig. 10), even if the values of the passive components are accurate. With the increase in  $Q$ , the size of the "the hump" increases to the appearance of oscillations. If the notch frequency is preset this can be rectified by adding an RC phase leading section at the input of the amplifier of Fig. 6 and experimentally adjusting the time constant. If the notch frequency must be variable, the only remedy is to use a wide bandwidth amplifier. However, at fairly high frequencies high  $Q$  inductors are available, and a passive filter such as the one in Fig. 3 may be preferable.

**Simulated inductance**

The circuit of Fig. 11(a) is an active bridge similar to that shown in Fig. 8(a), but has a series resonant circuit in one of its arms. If  $R_1/R_2 = r_1/r_2$ , the circuit will behave as a notch filter whose rejection frequency and factor of merit are

$$\omega_0 = 1/\sqrt{LC_1} \text{ and } Q_0 = \omega_0 L/R_2 \quad (6)$$

In order to avoid using an inductance, the series connection of  $R_2$  and  $L$  can be replaced by the circuit of Fig. 11(b)<sup>4</sup> which is equivalent to a coil whose value is  $L = C_2 R_2 \alpha(1-\alpha)$  in series with a resistor  $R_2$ . The resulting notch filter has a rejection frequency and factor of merit given by:

$$\omega_0 = 1/\sqrt{C_1 C_2 R_2^2 \alpha(1-\alpha)} \text{ and } Q_0 = \alpha(1-\alpha) \sqrt{C_2/C_1} \quad (7)$$

respectively; the tuning law is thus exactly the same as that of Fig. 2(c).

This network can also be tuned by means of  $C_1$ , which may consist of a small trimming capacitor if the simulated inductance is made appropriately large.

**State variable filters**

A unique active notch filter may be realized by the so-called state variable method<sup>5</sup>. This method is based on a multiple feedback network containing integrators and adders. In spite of the rather large number of operational amplifiers, the number of capacitors needed for the realization of any arbitrary transfer function is minimal.

The basic building block shown in Fig. 12 simultaneously provides three transfer functions of the second order; these are high-pass, band-pass and low-pass function, given by:

$$V_H(s) = Ks^2/(s^2 + (\omega_0/Q_0)s + \omega_0^2) \quad (8)$$

$$V_B(s) = K \frac{-\frac{1}{\tau_1} s}{s^2 + \frac{\omega_0}{Q_0} s + \omega_0^2}$$

$$V_L(s) = K \frac{\omega_0^2}{s^2 + \frac{\omega_0}{Q_0} s + \omega_0^2}$$

The resonant frequency  $\omega_0$  is determined by the time constants  $\tau_1, \tau_2$  of the integrators, and is given by  $\omega_0 = 1/\sqrt{\tau_1 \tau_2}$ . The factor of merit is  $Q_0 = 1/K \sqrt{\tau_2/\tau_1}$  where  $K = 1/(1 + R_F/2R_Q)$ .

This configuration does not provide complex zeros and in order to obtain

the symmetric notch response given by expression (1) we must sum the high-pass and low-pass outputs. The filter obtained contains four operational amplifiers but has the following characteristics: if  $\tau_2$  varies, the rejection frequency is varied while the bandwidth  $\Delta\omega = \omega_0/Q_0$  remains unchanged; if  $\tau_1$  and  $\tau_2$  vary simultaneously, the rejection frequency varies linearly while the factor of merit  $Q_0$  remains unchanged; if  $K$  is varied with the aid of the resistor  $R_Q$ , the rejection frequency remains unchanged and the rejection bandwidth and gain alone will change; the network is quite insensitive both to the values of the passive components and to the gain of the amplifier. Its stability approaches that of passive filters.

The transfer function of a conventional integrator is:  $G(s) = 1/\tau s = 1/RCs$  and the variation of  $\tau$  can be obtained by varying  $R$  or  $C$ . If we connect an amplifier with a gain  $K$  in series with the integrator, the transfer function changes to  $G(s) = K/\tau s$ ; i.e.,  $\tau$  is decreased without altering  $R$  or  $C$ . If an analogue multiplier is substituted for the amplifier, an integrator is obtained, in which the time constant  $\tau$  is dependent on a control voltage. A notch filter with a constant  $Q$  and rejection frequency directly proportional to the control voltage can thus be built from two such integrators.

It has already been mentioned that the maximum  $Q$  factor which can be obtained in an active filter realization is limited – for a given resonant frequency – by the bandwidth of the operational amplifier. The state variable method is no exception to this rule. Design considerations resulting from these limitations were discussed by Thomas<sup>6</sup>.

**Bandpass filter synthesis**

A common disadvantage which is probably shared by all accepted active bandpass realizations is that the bandwidth is inversely proportional to the midband gain; in other words an increase of  $Q$  is accompanied by a proportional rise in gain, which is often undesirable.

A different realization of bandpass filter is given in Fig. 13(a) based on the equation:

$$A\left(1 - \frac{s^2 + \omega_0^2}{s^2 + \frac{\omega_0}{Q}s + \omega_0^2}\right) = A \frac{(s/Q)\omega_0}{s^2 + \frac{\omega_0}{Q}s + \omega_0^2} \tag{9}$$

which results in a bandpass transfer function whose midband gain is independent of  $Q$ . The configuration operates as follows: at frequencies which are remote from  $\bar{\omega}_0$  the notch filter transmission is unity, and the input to the differential amplifier is zero. At frequency  $\omega_0$  the notch filter transmission is zero and the input to the amplifier is unity. As equation (9) shows, the resulting bandpass filter has the same  $Q$  as the notch filter. Now it is easy to realize notch filters in which the

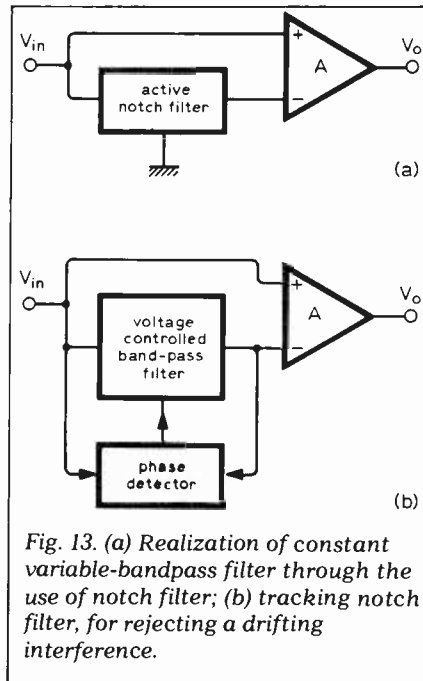


Fig. 13. (a) Realization of constant variable-bandpass filter through the use of notch filter; (b) tracking notch filter, for rejecting a drifting interference.

selectivity is controlled by a single resistor, such as the one shown in Fig. 8. If such a filter is incorporated, a constant-gain variable bandpass filter is obtained.

**Interference-tracking notch filter**

It has been previously mentioned that a sufficiently narrow-band notch filter may not be effective in rejecting interference which drifts in frequency. Such interference could in principle be tracked by a phase-locked loop, and the output of the loop, which is proportional to the frequency, then applied to a voltage-controlled notch filter. A drawback of such a method is that it is an open-loop system and any residual interference at the output due to imperfect tracking is not corrected for.

In contrast to the phase-locked loop, which is a signal-tracking oscillator, a signal-tracking band-pass filter can be easily built<sup>7</sup>. It is similar to the phase-locked loop and consists of a voltage-controlled band-pass filter, a phase detector and a low-pass filter. The closed loop then centres the band-pass filter on the signal by maintaining an (ideally) zero phase shift between the interference and the output of the filter. This bandpass filter can be converted to a signal-tracking notch filter as shown in Fig. 13(b), in which the filtered interference is subtracted from the original input. However, unlike conventional notch filters, the input to this filter must contain a minimum of interference for locking to occur.

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**Books Received**

**Dictionary of Data Processing** by Jeff Maynard is designed mainly as a source of reference for those interested in, or using computers and data processing equipment. Over 4000 terms are defined, as well as acronyms and abbreviations, in alphabetical order. The final section of the book lists British and American standards relating to data processing. Price £3.90. Pp.269. Butterworth & Co. Ltd, Borough Green, Sevenoaks, Kent TN15 8PH.

**Energy and Humanity** edited by M. W. Thring and R. J. Crookes, as a former US Secretary of Commerce has pointed out, a finite world with finite energy resources cannot support an exponential growth rate. This book presents the problem as it exists now, with a view to what might be the situation at the turn of the century. An attempt has been made to cover the existing sources of energy along with their associated problems and to assess what might become available in the future. Much of the material has been drawn from an international conference on energy and humanity, held by the SSRS in September 1972. Price £5.50. Pp.195. Peter Peregrinus Ltd, P.O. Box 8, Southgate House, Stevenage, Herts SG1 1HQ.

Recent, updated additions to the **D.A.T.A.** books range cover discontinued thyristors, m.s.i.-l.s.i. memories, diodes, linear i.c.s., microwave tubes, digital integrated circuits, and thyristors. As usual these books provide information on components from most of the producers in the world. Outline diagrams are provided together with pin configurations, and an index of manufacturers is also incorporated making these volumes an invaluable source of information. London Information Ltd, Index House, Ascot, Berks SL5 7EU.

**The International VHF-FM Guide** by Julian Baldwin and Kris Partridge. This booklet is a useful source of information for the radio amateur who wishes to operate through the VHF repeater networks both at home and abroad. Price 25p + 5p postage and packing. Pp. 38. J. E. C. Baldwin, 50 Aldbourne Road, Burnham, Slough, SL1 7NJ.

# Letters to the Editor

## "HIGH QUALITY F.M. TUNER"

I was most interested to see that the position of the ceramic filter in Mr J. B. Dance's f.m. tuner (March issue) was after the limiting amplifier. Surely if the filter is to aid tuner selectivity then it must be placed before those parts of the tuner which have non-linear transfer characteristics, i.e. before the limiting amplifier.

Assuming that the input signal level is sufficient to cause limiting (as it should be for any usable signal) then any spurious signal components emerging from the r.f. unit outside the desired i.f. bandwidth will be subjected to intermodulation by the limiting process. Any intermodulation products which appear within the i.f. bandwidth will not be removed by subsequent filtering, but will affect the audio output. Consider, for example the case where one is trying to receive a weak signal in the presence of strong signals in adjacent channels. The output of the r.f. section may contain levels of the adjacent channels of similar or greater amplitude than that of the required signal. In this design the limiter may act on these adjacent channel signals so that these subsequently affect the audio output. Placing the i.f. selectivity before limiting will reduce the levels of unwanted signals entering the limiter, and reduce audible effects due to them.

Intermodulation in the limiter may explain the poor performance observed by the author on an r.f. unit with a high level of local oscillator output.

Note that some filtering after the limiter may be necessary to avoid harmonics of the 10.7MHz i.f. signal affecting the operation of the second mixer.

J. E. Marshall,  
Bilborough,  
Nottingham.

*Mr Dance replies:*

I am grateful to Mr Marshall for raising an important point. The NE563 limiter has a bandwidth of 22MHz (typical) and a gain of 60dB. The filter placed between the limiter output and the mixer will

reject any noise which lies outside the required passband and will also attenuate any harmonics generated in the limiter.

If one wishes to have a tuner which provides optimum reception of weak signals in a crowded band, then additional filtering is required before the limiter. However, the front-end specified in my article contains a double tuned 10.7MHz circuit before the emitter follower output stage and I felt that the overall selectivity was adequate for normal domestic reception.

I did experiment with an additional FM-4 filter between the front-end and the limiter input. This involved the use of a matching resistor (270 ohm) between the front-end and the filter and a 330 ohm resistor on the output side of the filter. An active circuit is required between the filter output and the limiter, since the input impedance of the latter is quoted as 135 ohms. An active circuit providing gain will also improve the a.m. rejection. However, it seemed that the published circuit was satisfactory for domestic reception and I felt its simplicity would appeal to many readers.

With reference to Mr Marshall's penultimate paragraph, I did try an extra FM-4 filter with the front-end which gave unsatisfactory results, but I still did not obtain audio output of satisfactory quality.

Dr A. Tip of FOM-Instituut Voor Atoom-En Molecuulfysica, Amsterdam, has kindly sent me details of his unpublished work with a more complex system which he uses to receive many UK transmissions. Unfortunately only a few brief details can be mentioned here. Dr Tip employs a BFY90 amplifier by his aerial, and a Valvo FD1A front-end which feeds a 3028A variable gain cascode stage. Four ceramic filters are used, followed by a LM733 stage (set for a gain of 100); the latter feeds the NE563 limiter. The a.g.c. output from the NE563 is fed to a transistor amplifier which provides a.g.c. for the 3028A stage; the amplified a.g.c. also feeds a signal strength meter which is unaffected by the setting of the 563 muting circuit.

In conclusion, may I mention that the NE563 masks are being modified in California? The new NE563 devices will have a different oscillator impedance and should operate more reliably with the Taiyo CR-9.8 ceramic resonators mentioned in my article; the parallel 2.2kilohm resistor and 5pF capacitor should not be required with the new NE 563. In addition, Signetics expect the new device will produce an output with less distortion, but no figures are available at the time of writing. In their current data Signetics suggest a value of 5.1 kilohm for  $R_6$  of my Fig. 1; this will give a slightly improved signal-to-noise ratio and a reduced bandwidth, but the difference is not very noticeable.

J. B. Dance,  
Alcester, Warwickshire.

## SILENT STEREO SWITCH

Mr Moulana's article in the January 1975 issue, involving the use of f.e.t.s for audio switching, prompts me to raise a couple of points:

(1) Using a switching f.e.t at the virtual earth point of an inverting amplifier in series with the input arm (as shown in Fig. 1) ensures low voltage swings at the

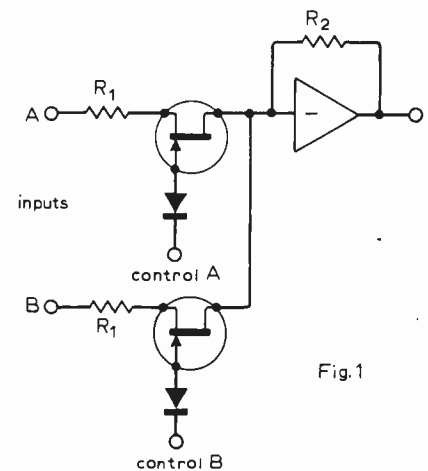


Fig. 1

f.e.t. and takes care of biasing. This configuration is often used in audio equipment.

(2) It seems reasonable that an f.e.t. with a low value of  $r_{ds(on)}$  should have a variation in this resistance with  $v_{ds}$  that is also of a low order (in absolute, if not proportional terms). Thus if an f.e.t. such as a TIS73L (Texas) is chosen, which has an  $r_{ds(on)}$  of 25 ohms maximum, we can see that the variation in  $r_{ds(on)}$  can be quite small.

Suppose that in the circuit of Fig. 1 we use the TIS73L, and make  $R_1 = R_2$  (for unity gain) = 10k $\Omega$ , then a variation in  $r_{ds(on)}$  of 20% (5 ohms) due to changing  $v_{ds}$  will give a rise to a distortion of approximately  $5/10^4$ , or 0.05%. Attenuation of the input signal by 20dB, and making  $R_2 = 100k\Omega$  will obviously improve the distortion performance while retaining unity gain. Pinch-off voltage for the TIS73L is a maximum of -11 volts, therefore control voltages in the off mode should be at least -12 volts. Choice of input arm resistance can

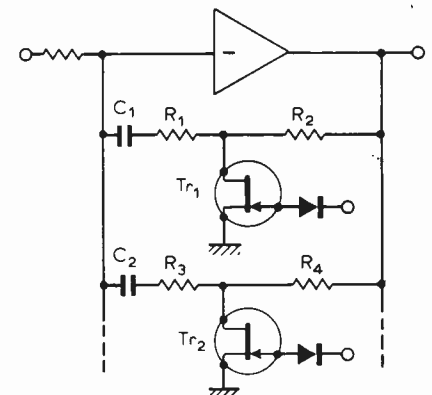


Fig. 2

optimize on/off ratio on the one hand, distortion and input impedance on the other.

As a postscript, a useful configuration when, for example, equalizations are to be switched, is shown in Fig. 2. In this circuit, using low impedance termination of the feedback networks at both ends, the required equalization time constant,  $(R_1 + R_2)C_1$  or  $(R_3 + R_4)C_2$  in Fig. 2, is selected by turning the f.e.t ( $Tr_1$  or  $Tr_2$  respectively) off, and all others on. Thus all feedback paths except that required are shunted to ground. If  $R_1, 2, 3, 4$  are of the order of  $100k\Omega$  and  $Tr_1$  and  $Tr_2$  are TIS73L, attenuation of the unwanted f.b. is  $(25 + 100k)/25$ , greater than 70dB. Distortion is low because the selected f.b. path uses an f.e.t. in the "off" mode, and contributions from f.e.t.s in the "on" mode are at very low level.

S. F. Bywaters,  
London, N.W.11.

## COMPUTER POWER

It is your privilege as editor to don the mantle of Cassandra from time to time; and we may have cause to be grateful to you for warning us (leader, May issue) of the latent threat of computer power.

Readers of your editorial may however care to join me as I hasten to bury my head in the sand. Or, as it might be, paper; since waste paper is the most obvious product of today's computers. What can be discovered in this mountain of paper is that a computer with remote terminal and interactive conversational language can take all the arithmetical grind out of hitherto laborious calculations in radio and electronics. And this generally involves only a minimal knowledge of computer programming - rather less, I suspect, than is currently mastered by schoolchildren. Indeed, readers who have no direct access to such computing facilities might well bribe sons and daughters to compute for them.

There is of course an additional bonus in speed and accuracy. For example, given the radio frequency range required together with the intermediate frequency, one can calculate component values for superheterodyne tracking to an accuracy much higher than the tolerances of actual components in less than five minutes. A similar time is required to plot the actual tracking error curve. If one then requires information on where the tracking curve moves to at the limits of specified component tolerances, another five minutes will suffice. Most of this total of fifteen minutes is spent by the system in organising itself and in printing - actual computing time may be only two or three minutes.

The story is very similar if one wishes to perform calculations on coupled tuned circuits - the complex arithmetic takes much less time than printing the

(unnecessarily accurate) results.

Any reader who has problems with tedious calculations of this kind is welcome to contact me.

D. P. C. Thackeray,  
Department of Chemical Physics  
University of Surrey,  
Guildford, Surrey.

## ELECTRODYNAMICALLY INDUCED E.M.F.

"Cathode Ray's" article and Mr Meade's letter (February issue) have prompted some questions concerning a well known problem in school-boy physics:

"If an aeroplane flies a level course through a known vertical component of the earth's magnetic field, then its wings act as a flux cutting conductor and an e.m.f. is induced in them. Can this e.m.f. be measured and, hence, the speed of the aircraft deduced?"

The answer is, of course, no, because as "Cathode Ray" stated, connecting a voltmeter to the ends of the conductor (in this case the wings) would form a closed loop embracing a constant magnetic flux.

Not being well versed in the theory of electromagnetic induction, we would like to ask the following questions:

"Can the induced e.m.f. be measured if the meter leads are screened with a high permeability material?" and, naturally, "If not, why not?"

D. C. E. Todd and  
N. G. S. Taylor,  
Brunel University,  
London.

## DIRECTORY OF AUDIO COURSES

The Audio Engineering Society is preparing a Directory of educational facilities and institutions in its field of interest, which embraces sound recording and reproduction, instrumentation, sound reinforcement etc. This information will appear in the *Journal* of the AES and be included in a career booklet eventually to be prepared by the Society.

As the UK representative of the AES Education Committee, I have been asked to act as a focal point for the collection of such information from schools, colleges and universities in the British Isles.

To simplify the listings, I can supply copies of a short questionnaire and I would urge all organisers of courses related to audio engineering to apply to me for copies as soon as possible.

John Borwick,  
Senior Lecturer,  
Recording Techniques  
University of Surrey,  
Guildford,  
Surrey.

## INSTRUMENT READ-OUT IN BRAILLE?

I have recently become interested in the problems of teaching science to blind pupils. Present techniques offer analogue derived information in tactile or audible form. For example in typical science experiments one might wish to indicate the height of a liquid column or the reading of a meter. The liquid level would be located by a light probe whose audio tone would alter on discovering the surface; the meter pointer would be located either by the light probe or feeling the pointer in an instrument made specially for the blind. The actual reading is then taken from an adjacent Braille scale.

Of necessity these procedures are slow, clumsy and very approximate. It occurs to me that in the case of meter readings digital techniques could be exploited with considerable advantage. Many readouts are available in digital form - voltmeters, ammeters, frequency meters, multimeters, balances, calculators - and in many cases the electronics involves binary processing of numbers which in b.c.d. form is decoded for a visual readout such as a seven-segment device. Could not the b.c.d. be decoded direct to Braille format and used to operate a tactile display? It should be possible to devise an electromechanical Braille readout as only four pins are required as shown in the diagram. My guess, based on no direct experience, is that blind pupils would find the reading of electrical quantities more direct and so more meaningful. In the case of balances the accuracy of the weighing would certainly help science teaching. If it proved possible to use this idea with electronic calculator chips, perhaps a new era in teaching maths to the blind might follow also.

Recent progress in artificial vision, reported in your April issue, raises an even more powerful possibility, namely direct excitation of the optic nerve with numerical data. Whether this should be b.c.d., seven-segment, Braille, or some other format is a matter for speculation. Braille has already been used successfully (WW, April p.157) for text by this means.

J. M. Osborne,  
London, SE5.

	b.c.d.	denoted by Braille letter	A B D C	a binary equivalent of Braille
0	0000	J		0111
1	0001	A		1000
2	0010	B		1001
3	0011	C		1100
4	0100	D		1110
5	0101	E		1010
6	0110	F		1101
7	0111	G		1111
8	1000	H		1011
9	1001	I		0101

Binary coded decimal compared with numbers in Braille.

# Wireless World Dolby noise reducer

## 3 — Kit alignment and calibration

by Geoffrey Shorter

**Intended mainly for hiss reduction in magnetic-tape recording machines, this noise reduction unit can be switched to decode commercially-available Dolby B-encoded cassette tapes, Dolby B-encoded f.m. radio transmissions (current in the USA), or to encode blank tapes from any source. As an alternative it can be used in trading some of the noise improvement for reduced distortion at peak recorded levels. Part 1 in the May issue gave background to the Dolby system and part 2 gave circuit and constructional details together with some suggestions for circuit options and alignment procedure. This part shows how to set-up the kit version design without using additional equipment and gives calibration procedure.**

Constructors who build a Dolby-B processor without using the full WW kit have the option of using the power supply included in the circuit of Fig. 12 or of using an alternative one, for instance one built into existing equipment. Component values for the circuit of Fig. 12 have been optimized to provide an overload margin of 16dB (equivalent to 1200nWb/m on open-reel) for a 15-volt supply, but voltages between 15 and 24 volts could be used provided component voltage ratings are chosen appropriately. The main requirement is that supply ripple be less than 200 $\mu$ V r.m.s. Current consumption at 15 volts is 20mA per processor; with IC<sub>1</sub> and IC<sub>2</sub> it is 30mA. The voltage regulator IC<sub>2</sub>, whose output is 15 volts  $\pm$  5%, is essential if the meter calibration oscillator of Fig. 14 is used. Input to the regulator should be not greater than 25V and not less than 18.25V.

### Kit setting-up procedure

The procedure for setting up the kit design is a little more elaborate than the basic alignment instructions because it is designed to eliminate necessity for additional equipment i.e. a.c. millivoltmeter and variable-frequency a.f. oscillator. It therefore includes a facility for generating a 5kHz circuit alignment tone, as well as a 400Hz calibration tone. Two meter amplifiers, and a 580mV source (1kHz oscillator) to calibrate the meters, are included to obviate the need for an a.c. millivoltmeter.

In using the in-built meter scale in setting up, it is better to use close-tolerance resistors in an attenuator so that all measurements can be made at one meter reading (0dB). Errors in meter reading are minimized by this tech-

nique, and errors due to an inaccurate scale eliminated.

### Right-channel meter calibration

The unit is aligned using part of IC<sub>1</sub> as a meter calibration oscillator. The amplifier section of IC<sub>1</sub> based on pins 10, 11 and 12 is first used as shown in Fig. 14. In this mode the amplifier is wired as an astable multivibrator switching between the 15V supply rail and 0V, with a mark-to-space ratio of about 1:1 and a frequency of around 1kHz. The real voltage swing is a little less due to saturation voltages, but is highly repeatable from one sample to another.

### Typical performance

Noise reduction: better than 9dB weighted

Clipping level: 16.5dB above Dolby level (measured at 1% third harmonic content)

Harmonic distortion: 0.1% at Dolby level (typically 0.05% over most of band, rising to a maximum of 0.12%)

Signal-to-noise ratio: 66dB (20Hz to 20kHz, signal at Dolby level)

Approximate voltage readings (AVO 8)

	collector	emitter
Tr <sub>1</sub>	9.0	0.6
Tr <sub>2</sub>	14.3	1.5
Tr <sub>3</sub>	7.6	rail
Tr <sub>5</sub>	rail	7.6
Tr <sub>6</sub>	—	8.8
Tr <sub>7</sub>	8.4	rail
Tr <sub>8</sub>	8.0	2.6
IC <sub>1</sub>	pin 4	6.8V
	pin 5	7.7V

—Connect resistor R<sub>59</sub> (3.9M $\Omega$ ) from the pin at R<sub>51</sub> to pin 2 or the L<sub>2</sub>' position.

—Wire R<sub>58</sub> (10k $\Omega$ ) in parallel with R<sub>47</sub> (1M $\Omega$ ) across the pins at R<sub>47</sub> position.

—Form an attenuator with R<sub>60</sub> (110k $\Omega$  2%) and R<sub>61</sub> (10k $\Omega$  2%) in series, Fig. 14, earthing the end of R<sub>61</sub> by connecting to pin 3 of L<sub>2</sub>' and connecting R<sub>60</sub> to pin 1.

—Solder one end each of R<sub>55</sub> (330k $\Omega$  2%) and R<sub>155</sub> (330k $\Omega$ ) to their pins. Take the other end of R<sub>55</sub> to the junction of R<sub>60</sub>, R<sub>61</sub> (R<sub>155</sub> remaining floating). Switch on.

—Adjust RV<sub>8</sub> (Fig. 15) until the r.h. meter reads 0dB. Switch off.

—Remove R<sub>55</sub>, R<sub>58</sub>, R<sub>59</sub>, R<sub>60</sub>, R<sub>61</sub> and do not alter the setting of RV<sub>8</sub>.

### Circuit alignment

The now-calibrated r.h. meter is used to set the gain and f.e.t. bias controls of both left and right processors with the help of a 5-kHz oscillator, Fig. 14, adapted from the 1-kHz oscillator circuit by using arrangement (b).

—Solder C<sub>30</sub> in position, removing and replacing the p.c.b.

—Solder L<sub>2</sub> on to pins 1 and 2 of the L<sub>2</sub>' position. Gently screw in the core.

### Right-channel circuit alignment.

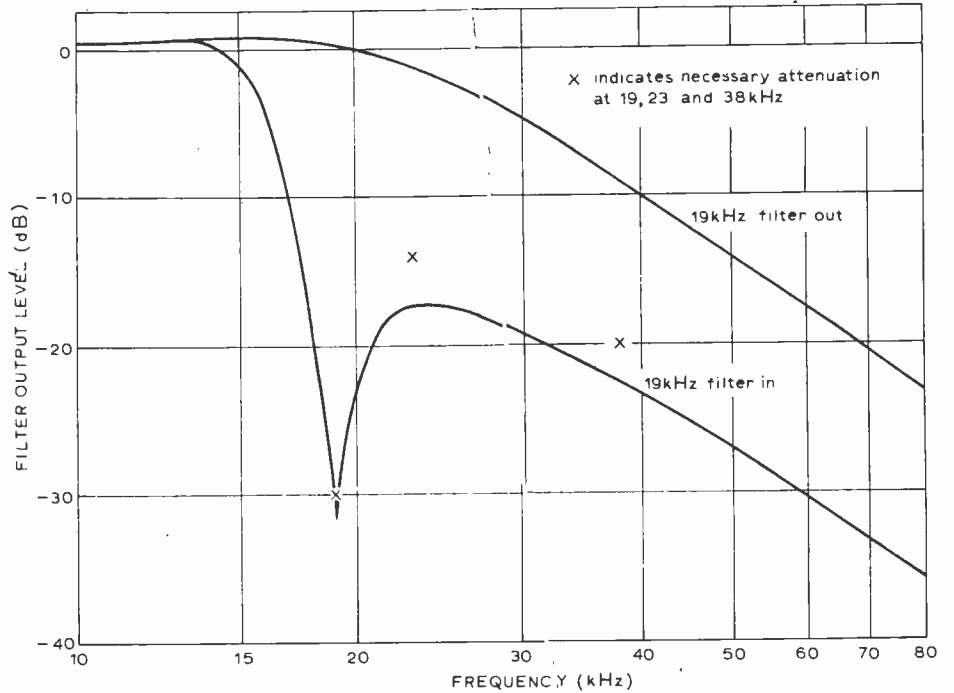
—Connect R<sub>61</sub> (10k $\Omega$  2%) between the R<sub>55</sub> pin and test point 1 (TP1) on the sub-board.

—wire the oscillator pin, marked "osc." to the sub-board pin marked R' (input to processor).

—Set RV<sub>5</sub> (oscillator level) fully anticlockwise. Check that no plugs are connected into the sockets.



- Set  $RV_{2,102}$  fully anticlockwise. Switch on.
- Select the auxiliary position for  $Sw_2$ . Set the balance control  $RV_9$  to mid-position and the input level control  $RV_{10}$  fully clockwise.
- Ensure the calibration tone switch  $Sw_3$ , the noise reduce switch  $Sw_4$ , and the 19-kHz filter switch  $Sw_6$  are in the off position (out), and the check tape switch  $Sw_5$  is in the normal position (out).
- Check that the f.e.t. gates have previously been shorted to ground by two looped links.
- Turn the law control  $RV_1$  fully clockwise to pinch-off f.e.t.
- Switch  $Sw_1$  to record and adjust  $RV_5$  until the meter reads 0dB (equivalent to 17.5mV at TP1). Switch off.
- Transfer the end of  $R_{61}$  from TP1 on the sub-board to TP2 and switch on. Meter should read within  $\pm 1$ dB of the previous, 0-dB reading. Note actual reading \*. Switch off.
- Solder  $R_{62}$  (15k $\Omega$  2%) and  $R_{63}$  (6.8k $\Omega$ ) in series with  $R_{61}$  (i.e. between the  $R_{55}$  pin and TP2), decreasing meter sensitivity by 10dB. Switch on and check meter reading reduces by roughly two thirds.
- Switch on noise reduction,  $Sw_4$  and



Amplitude response with and without 19kHz filter.

Fig. 18. First part in setting-up procedure for kit version (left) shows arrangement used in calibrating the right-channel meter. For aligning the noise reduction circuit the meter calibration oscillator is changed to a 5kHz oscillator, using  $L_2$  temporarily in the  $L_2'$  position (centre). Its output, via the "osc" pin, is taken to the processor input (R' for the right channel). To calibrate the 400Hz oscillator,  $L_2$  is put in its normal position, the i.c. oscillator disabled, and the oscillator output taken from TP1 or TP101 (right).

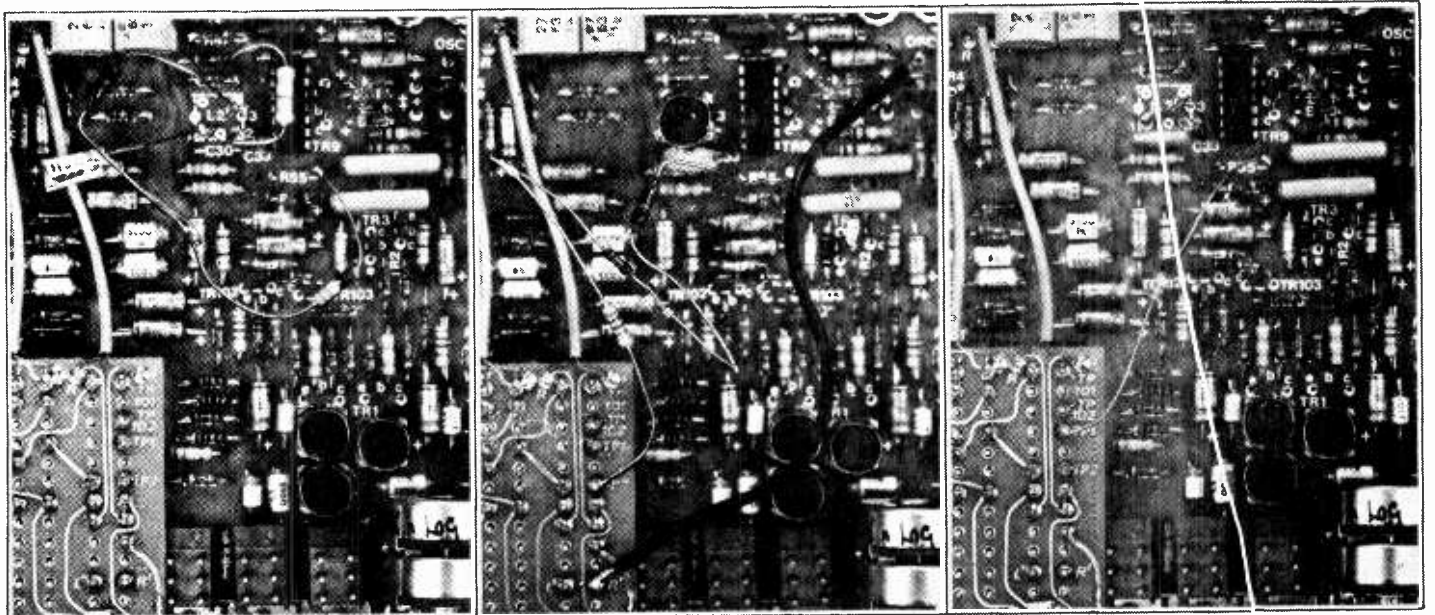
- adjust  $RV_2$  (gain) to bring back meter reading to that noted above at \*. Switch off.
- Cut the f.e.t. gate short for the right-hand channel with wire cutters and short-circuit  $R_{63}$  increasing meter sensitivity by 2dB. Switch on.
- Adjust  $RV_1$  (law) until meter reads as noted above, at \*. Switch off.
- Re-apply f.e.t. gate short and replace  $R_{63}$ . Switch on and check meter still reads as above, at \*. Switch off. Remove gate short.

**Encode/decode matching check.**

- Switch  $Sw_1$  to play and switch noise reduction off,  $Sw_4$ .
- Short-circuit  $R_{63}$ , leaving  $R_{61}$  and  $R_{62}$  connected. Set  $RV_{4,104}$  fully clockwise. Switch on.
- Adjust 5-kHz oscillator output level control  $RV_5$  until meter reads 0dB

- (equivalent to 44mV at TP2). Switch off.
- Switch noise reduction on,  $Sw_4$ . Short-circuit  $R_{62}$  and  $R_{63}$  so that only  $R_{61}$  is in circuit. Switch on. Meter should read 0dB to within  $\pm 1$ dB. Switch off.

**Left-channel circuit alignment.** Now repeat this process for the left channel, starting from the point of connecting  $R_{61}$  between the  $R_{55}$  pin, (not  $R_{155}$ ) and the test point — now to be TP101 — on the sub-board. Note that the right channel meter, being calibrated, is still used in setting up the left channel, and that TP101 is to be read for TP1, TP102 for TP2,  $RV_{101}$  for  $RV_1$ ,  $RV_{102}$  for  $RV_2$ , and that the left-channel f.e.t. gate-shorting loop is now implied. The "osc" pin is to be connected to the point L' on the sub-board at the appropriate time.



After repeating for the left channel, switch off. The gain and law adjustments are now complete.

- Remove the f.e.t. gate shorts,  $R_{61}$ ,  $R_{62}$  and  $L_2$ , inserting  $L_2$  into its normal (final) location.

#### 400Hz oscillator calibration

- Solder one end of  $R_{55}$  to its pin and connect the other end to TP1.
- Short pins 1 and 3† at the  $L_2'$  position, and remove the wire from osc pin to point L'. Switch on.
- Switch  $Sw_1$  to record, press the noise reduce switch  $Sw_4$  off and switch on the 400-Hz calibration tone oscillator,  $Sw_3$ .
- Adjust  $RV_3$  (oscillator level) until the right-channel meter reads 0dB. Switch off.
- Transfer the end of  $R_{55}$  from TP1 to TP101 and switch on. Adjust  $RV_{103}$  until the r.h. meter reads 0dB.
- Repeat this procedure because of a slight interaction between  $RV_3$  and  $RV_{103}$ . Switch off.

#### Left-channel meter calibration

- Disconnect  $R_{55}$  from TP101 and connect the free end of  $R_{155}$  to TP101 and switch on.
- Adjust  $RV_{108}$  to obtain 0dB at the left-channel meter, being careful not to disturb  $RV_8$ . Switch off the cal. tone oscillator. Switch off.

†Experience has shown that a better method of disabling the 5kHz oscillator is to remove  $R_{47}$ .

#### 19kHz filter adjustment

- Wire  $R_{155}$  permanently onto the main board, replace  $R_{55}$  with  $R_{61}$  and connect free end to TP1.
- Connect an f.m. stereo tuner to the auxiliary input and with the aux-tuner links wired in, switch on and tune to a BBC stereo test transmission.\*

Alternatively, if a high accuracy ( $\pm 50$ Hz) 19kHz oscillator is available, connect its output to point R' on the sub-board.

- With zero a.f. modulation,\* adjust the record level control  $RV_{10}$  to give a 0dB meter reading. Switch the 19kHz filter on,  $Sw_6$ .
- Adjust  $L_2$  for minimum reading on the right-channel meter. Do not adjust  $L_1$  or  $L_{101}$ . Increase record level for sharper null near tuning point.

Repeat for the left channel starting by transferring end of  $R_{61}$  from TP1 to TP101, and adjusting  $L_{102}$  for minimum reading. (In using a 19kHz oscillator, connect to point L' on the sub-board and transfer  $R_{61}$  lead from TP1 to TP101 before adjusting  $L_{102}$ .)

#### Calibration

To ensure interchangeability of all Dolby B-encoded tapes and of Dolby

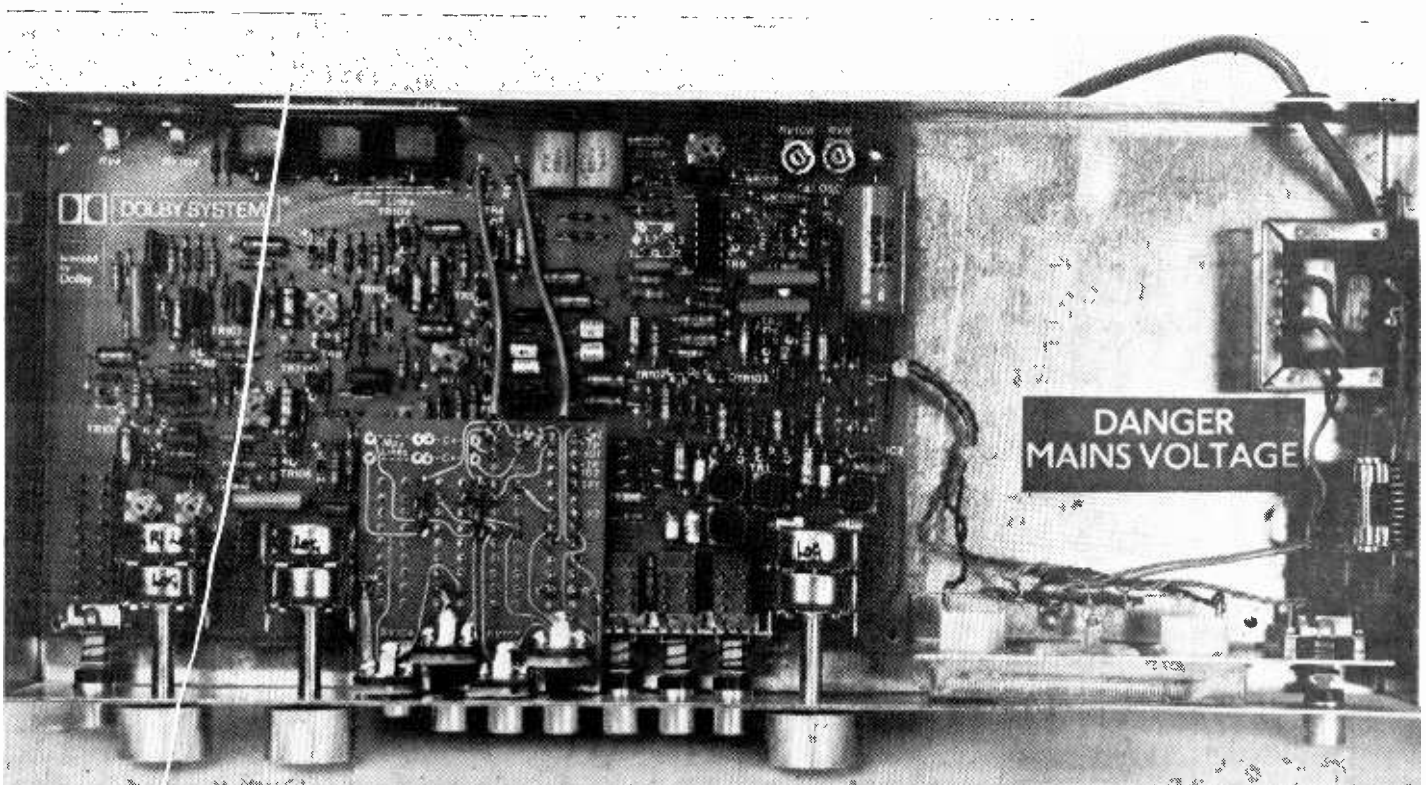
\* Stereophonic test transmissions are broadcast about four minutes after the close of Radio 3 programmes on Mondays and Saturdays. The zero a.f. modulation part occurs about 11 minutes after the start and lasts for nearly two minutes.

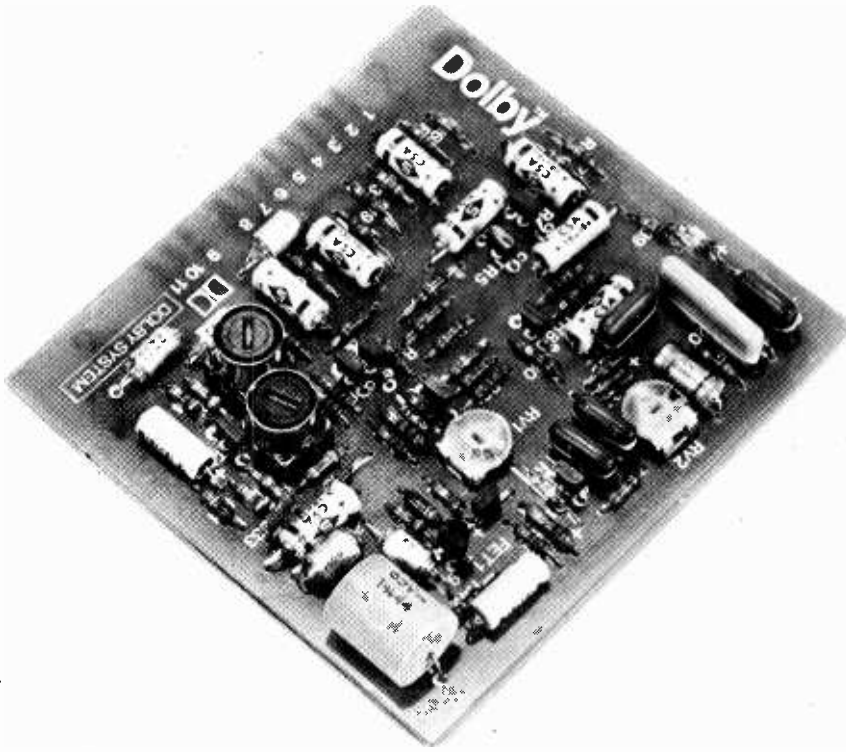
B-equipped machines, the voltage levels in the processors must be related to flux levels on the tape. A certain amplitude level is used that bears a fixed relationship to the noise reduction parameters and to conditions between encoder and decoder. The level chosen corresponds with a flux on open-reel tapes and cartridges of 185nWb/m, with 200nWb/m for cassette tapes, with a deviation of 37.5kHz on f.m. transmissions, and with a voltage level at the processor output of 580mV r.m.s.

This level, often called Dolby level, should not be taken to imply an operating level. If the level-setting meters in the unit are to be used as modulation-depth meters, a mark may be made on the meter to indicate the reference level. Whilst setting this level equal to 0VU on meters can often lead to reasonable modulation depths, this is not always the case: for cassette recorders it is best set at +3VU.

The 400Hz oscillator and tapes recorded with a 400Hz tone to the above level are used in calibrating units, once the circuitry has been set up. When playing or recording the standard flux level, the 580mV level is set by adjusting the play calibration potentiometers during play, and the record calibration potentiometers during recording.

**Playback-only decks and units.** As the signal levels on encoded tape cassettes are to be related to those in the decoder during playback only, the 400Hz oscillator is not required and calibration is achieved with a calibration cassette, containing the reference flux.





An alternative to the kit design is this single-channel processor, using the circuit of Fig. 12 but excluding power supply, alignment and calibration circuitry. (Track diagram will be given in a subsequent issue.)

- Switch noise reduction off.
- Play calibration tape. Set play gain control on tape deck to 0VU on deck meter, if possible, or to mid-position otherwise.
- Adjust play cal. control for 580mV on meter or Dolby level indication, depending on meter used.

Playback gain controls on the recorder in the signal path en route to the processor input should not now be disturbed.

#### Switchable encode/decode processors.

##### Playback calibration

- Switch to play and switch off noise reduction. Connect millivoltmeter to point G if meters not built-in.
- Play calibration tape. Set play gain control on tape deck if fitted to 0VU on deck meter, if possible, otherwise to mid-position.
- Adjust play cal. control for 580mV indication.

This completes playback calibration and the play gain controls on the tape deck should not be altered. Adjust listening level with the output level control following the decoder output (as in Fig.13).

##### Record calibration

Start by setting record gain control on tape deck to mid-position, if fitted. (If combined with playback gain, do not adjust.)

- Switch to record.
- Fit blank tape (as recommended by maker or for which bias is correctly adjusted) and feed in 400Hz at points from external or internal oscillator. (If unit has been built into cassette machine and 400Hz input is via line input socket, adjust record level control so that meter reads 580mV, or Dolby level.)
- Record on tape for a few seconds, rewind and playback, switching to play on the noise reduction circuit as well as on the deck. Note whether meter shows about or below 580mV, or Dolby level.
- Make small adjustment to record cal. controls in appropriate direction and record 400Hz tone again, observing meter reading on playback. Repeat this procedure as many times as necessary to obtain correct reading.

This completes record calibration for tapes. If the circuit of Fig.13 or similar has been adopted, recording level is adjusted with record balance and level controls on the noise reduction unit, the level being judged by the tape deck's normal meters.

When the noise reduction unit is connected to a three-head machine with a simultaneous monitoring facility the tape signal may be monitored in its encoded form by operating the check tape switch.

**Simultaneous encode/decode circuits.** Constructors with three-head machines having a simultaneous monitoring

facility can use single-processor boards permanently wired in the encode and decode modes. If provision for encoded f.m. transmissions is required switching must be arranged so that encoding does not take place during recording. A monitor switch can be provided at the input to the decoder, to switch from tape, via a play cal. potentiometer, to source i.e. a connection to the encoder output via a 580-30mV attenuator, Fig 19.

Playback calibration procedure is as above, but record calibration is simplified.

- Set record level controls on tape recorder to mid-position. Set monitor switch to tape.
- Record on blank tape, operating the calibration tone switch or injecting a 400Hz tone from an external oscillator.
- Adjust record cal. control so that meter reads 580mV, or Dolby level.

**FM calibration.** If you wish to set the controls for encoded f.m. transmissions, currently being transmitted by stations in the USA, an approximate calibration can be achieved by tuning to a local station, switching to f.m. or Dolby f.m. and setting the f.m. cal. control to give meter readings similar to those obtained when playing pre-recorded tapes. More accurate adjustment can be obtained if a station can be received which transmits the 400Hz calibration tone, identified by a characteristic warbling, or alternatively by using an f.m. generator. In this last-mentioned case, modulation frequency should be set to about 400Hz with a peak deviation of 37.5kHz (not including pilot tone).

#### Change of time-constant for encoded f.m. transmissions

There are two commonly used pre-emphasis time constants, 50 $\mu$ s and 75 $\mu$ s. Under certain conditions, these values can lead to reduced modulation at low and medium frequencies or severe amplitude distortion at high frequencies. In the USA the FCC has approved Dolby Laboratories' proposal of using 25 $\mu$ s for encoded transmissions, and to receive such broadcasts it is necessary to alter the de-emphasis time constant. In the circuit of Fig.13 this is achieved with components R<sub>x</sub> and C<sub>x</sub>, values being given in the components list on page 259 (June) for the change from 75 to 25 $\mu$ s and for a change from 50 to 25 $\mu$ s (not yet authorized in 50 $\mu$ s countries). When recording such broadcasts the encoding function of the noise reduction unit is clearly not required and the "Dolby f.m." switch position automatically switches off the encoding function. Application of the Dolby B system to f.m. broadcasting is discussed in two articles in the *Journal of the Audio Engineering Society*, June 1973, pp.351-62, and briefly in the July 1974 issue of *Wireless World*, page 237.

- Tune in to whichever of these signals is available.
- Switch to record, and to either f.m. or Dolby f.m.
- Adjust f.m. cal. control so that meter reads 580mV, or Dolby level.

### Using the unit

The calibration procedures described theoretically apply to the one tape speed used during calibration. Whether the calibration will hold for different tape speeds depends on the design of the deck, so check calibration when speed is changed. The calibration tape available can be used at 4.75 and 19cm/s, as well as 9.5cm/s. (For 38cm/s tape speed, where the noise spectrum is wideband, applying the B-type system may result in the remaining mid and low-frequency noise becoming more apparent). When the brand of tape is changed it is usually necessary to readjust the record cal. controls, the play cal. setting remaining unchanged. The characteristics of cassette tapes are more critical, and changing brand will normally require adjustment of bias (and equalization when using CrO<sub>2</sub> tapes).

When the unit is connected to the normal input and output points of a tape recorder, the recorder's own input and output controls from part of the calibrated system. The settings used during calibration should not be disturbed,

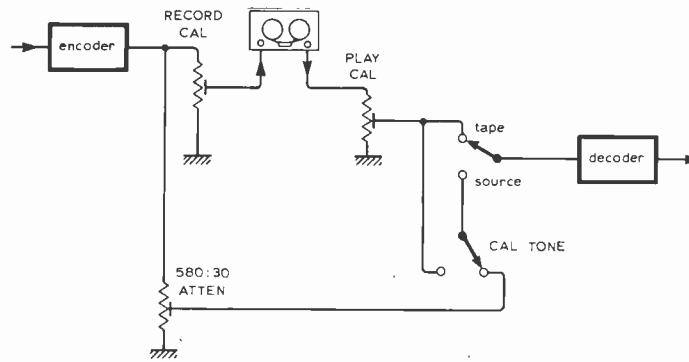


Fig. 19. Monitor switch arrangement for permanently-wired processors in three-head machines.

input and output level controls being provided on the noise reduction unit, and it is a good idea to mark the tape recorder control settings.

The amplitude response of the tape recorder must be flat and its gain unity, measured between point G of the processor in record and play, to ensure correct operation, so that the signal voltage in the decoder is the same as that at the encoder (to within 2dB). If there is a bandwidth restriction between encoder and decoder, e.g. if the response of the recorder does not extend up to at least 10kHz, a non-complementary situation arises, unless of course the encoder input bandwidth is similarly limited.

In using the unit don't forget that it will only reduce noise generated after

the encoder and before the decoder. If the input signal is noisy in itself or is made noisy by poor circuitry prior to encoding, this noise will be reproduced unaltered along with the signal. In some cassette decks, the line inputs are attenuated prior to amplification by a sometimes noisy microphone pre-amplifier.

As the sensitivity of the processor is of the order of 30mV, a line input amplifier is not required when the circuits are built into a tape recorder, and the input signal should be taken directly to the input gain control via a switch, or socket with switch, to disconnect the microphone pre-amplifier. It's a good idea too to make sure any automatic level limiter operates only in the microphone input and not in the line input.



Complete kits for the *Wireless World* Dolby B noise reducer are available through the address given below. The two-channel design features:

- a weighted noise reduction of 9dB
- switching for both encoding (low-level h.f. compression) and decoding
- a switchable f.m. stereo multiplex and bias filter
- provision for decoding Dolby f.m. radio transmissions (as in USA)
- no equipment needed for alignment
- suitability for both open-reel and cassette tape machines
- check tape switch for encoded monitoring in three-head machines

The kit includes:

- complete set of components for a stereo processor
  - regulated power supply components
  - board-mounted DIN sockets and push-button switches
  - fibreglass board designed for minimum wiring
  - solid mahogany cabinet, chassis, two meters, front panel, knobs, mounting screws and nuts.
- Price is £43 inclusive.

A single-channel printed-circuit board, with f.e.t. costs £2.50 and £8.63 with all components inclusive (excluding edge connector, £1.37 extra). Selected field-effect transis-

tors cost 68p each inclusive, £1.20 for two and £2.20 for four.

Calibration tapes are available, costing £1.94 inclusive for 9.5cm/s open-reel use and for cassette (specify which).

Send cash with order, making cheques payable to IPC Business Press Ltd, to:

Wireless World noise reducer  
General sales department  
Room 11, Dorset House,  
Stamford Street  
London SE1 9LU  
Allow three weeks for delivery.

# A 50 MHz oscilloscope

## 3 — E.h.t. oscillator, power supply and tube circuit

by C. M. J. Little, B.A.

Department of Electronics, Southampton University

The requirements of the c.r.t. are a negative supply of 1kV with a current capability of 2mA at maximum brilliance, and a positive supply of 3kV, at a current of 50 $\mu$ A. The e.h.t. supply must be stabilized in order to avoid changes in X and Y plate sensitivities with brilliance. Some oscilloscope designs use mains-derived e.h.t. and rely on the large current capability of the supply to avoid changes in voltage with loading. There are two major disadvantages of this system. First, the need for large-value smoothing capacitors, and second, the danger of lethal electric shock. This design uses the alternative, which is a transistor inverter operating at about 20kHz. Smoothing is easy at this frequency, and feedback stabilization can be used.

### E.h.t. generator

The circuit is shown in Fig. 11. Tr<sub>82</sub> and Tr<sub>83</sub> form a current-switched class D oscillator. This type of circuit produces

a sine wave, but has the high efficiency usually associated with square-wave inverters. The transistors act as switches with, ideally, zero voltage across the transistor for half the cycle. The waveforms are illustrated in Fig. 12. L<sub>7</sub> provides a constant current at the frequency of oscillation, and is uncritical as to exact value. The criterion is that its impedance at the working frequency should be large compared with the static resistance of the oscillator (supply voltage divided by supply current). The output voltage of this type of oscillator is very dependent on load.

The transformer T<sub>2</sub> resonates with its stray capacitance at about 18kHz. The secondary winding steps up the voltage to about 1.5kV peak, which is rectified to give -1kV d.c. and voltage trebled to give about +3kV d.c. The loading on the negative peaks is much greater than that on the positive so the trebler gives a higher voltage than one would expect. The feed to the stabilizer is taken from C<sub>128</sub> in order to avoid including the extra

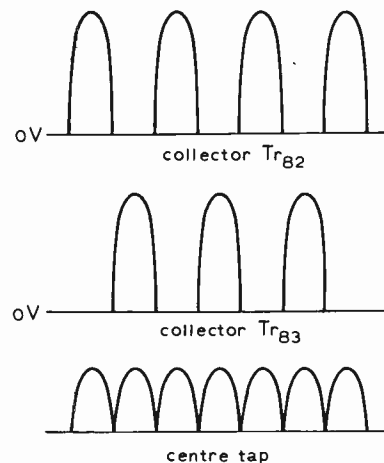
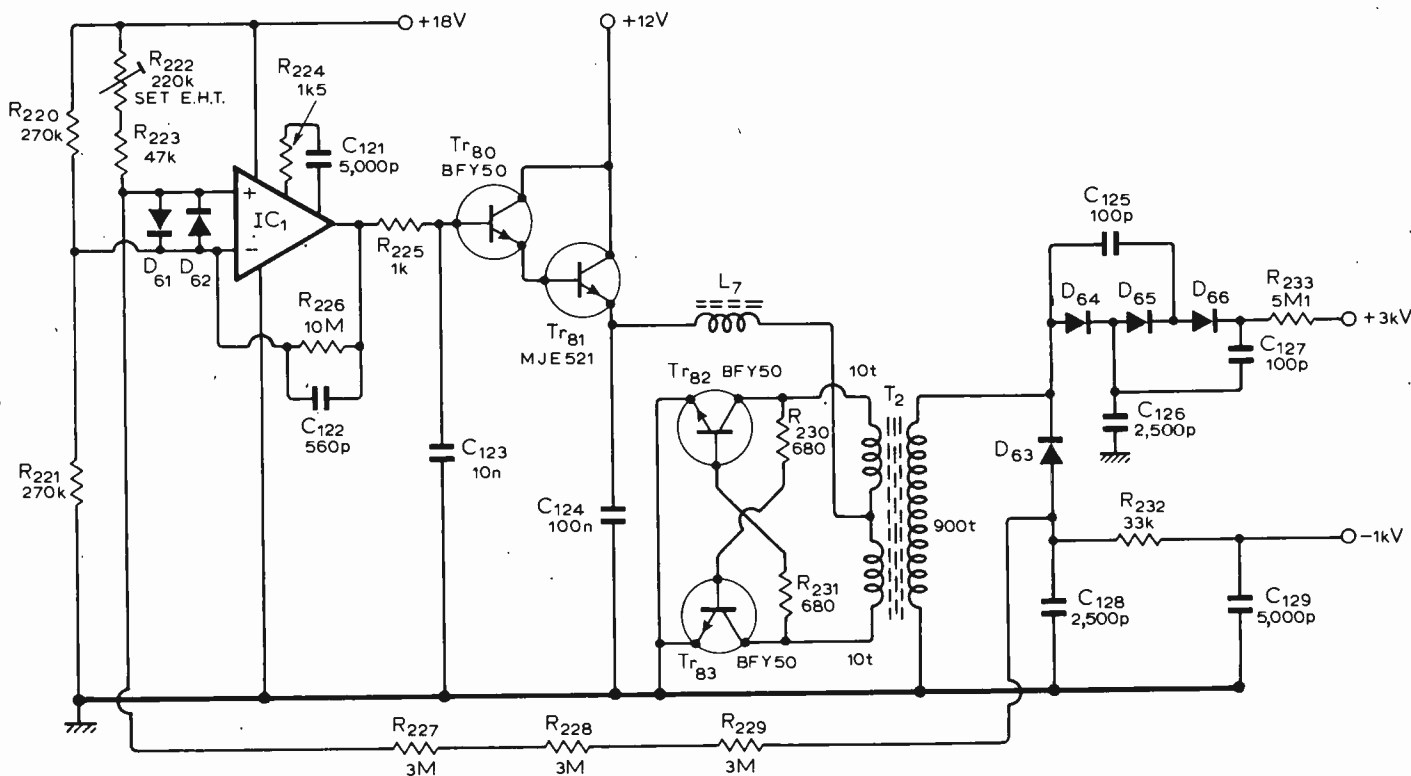


Fig. 12. Waveforms in the e.h.t. class D oscillator.

Fig. 11. The e.h.t. generator.





pole  $R_{232}$  and  $C_{129}$  in the feedback loop.

The error amplifier is an integrated operational amplifier with current multiplication provided by  $Tr_{80}$  and  $Tr_{81}$ . The amplifier is used in non-inverting mode and the negative e.h.t. is compared with the 18V rail.  $R_{226}$  and  $C_{122}$  provide a dominant pole at 30Hz. The gain at 50Hz is high enough to eliminate mains hum from the e.h.t. voltages. If a 741 type of amplifier is used instead of a 709,  $R_{224}$  and  $C_{121}$  may be left out.  $C_{124}$  is probably unnecessary and could be left out, as the effect of  $C_{123}$ ,  $Tr_{80}$  and  $Tr_{81}$  will be equivalent to a large capacitor at this point.

**C.r.t. and blanking**

The circuit associated with the cathode ray tube and the blanking amplifier are shown in Fig. 14. Before considering these, I would like to make some comments regarding the c.r.t. used in the instrument.

Of all the parts in an oscilloscope, the c.r.t. is the most critical, and the choice of tube will affect the performance that it is possible to obtain, and also the circuit techniques used. For these reasons I chose a currently available c.r.t. of modern design, instead of trying to find a surplus tube that might be satisfactory.

The c.r.t. specified has many modern features, such as a flat rectangular screen, built-in parallax-free graticule, spiral p.d.a. (post deflection acceleration) and high deflection sensitivities. It also has a second grid so that retrace blanking may be applied at earth potential. This greatly simplifies the blanking amplifier.

The penalty to be paid for this high performance, of course, is cost. The c.r.t., Mumetal shield, and base will cost about £40. For those readers who would otherwise hurriedly stop reading this article, I will now give some suggestions for possible use of surplus tubes.

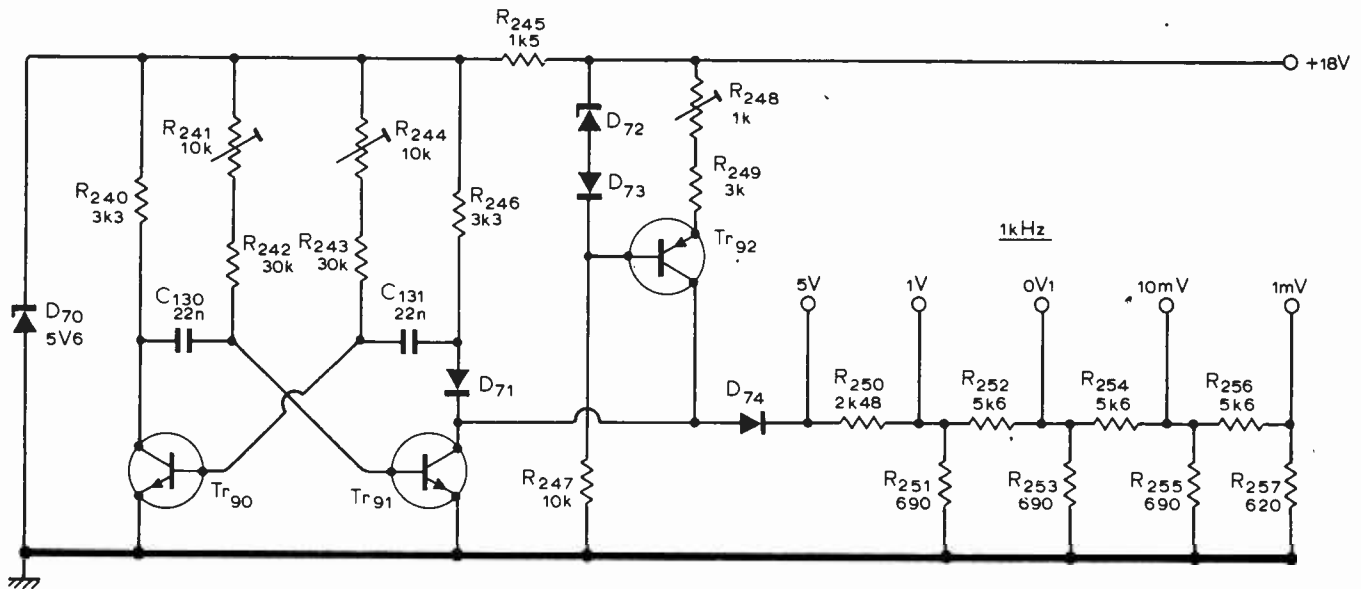
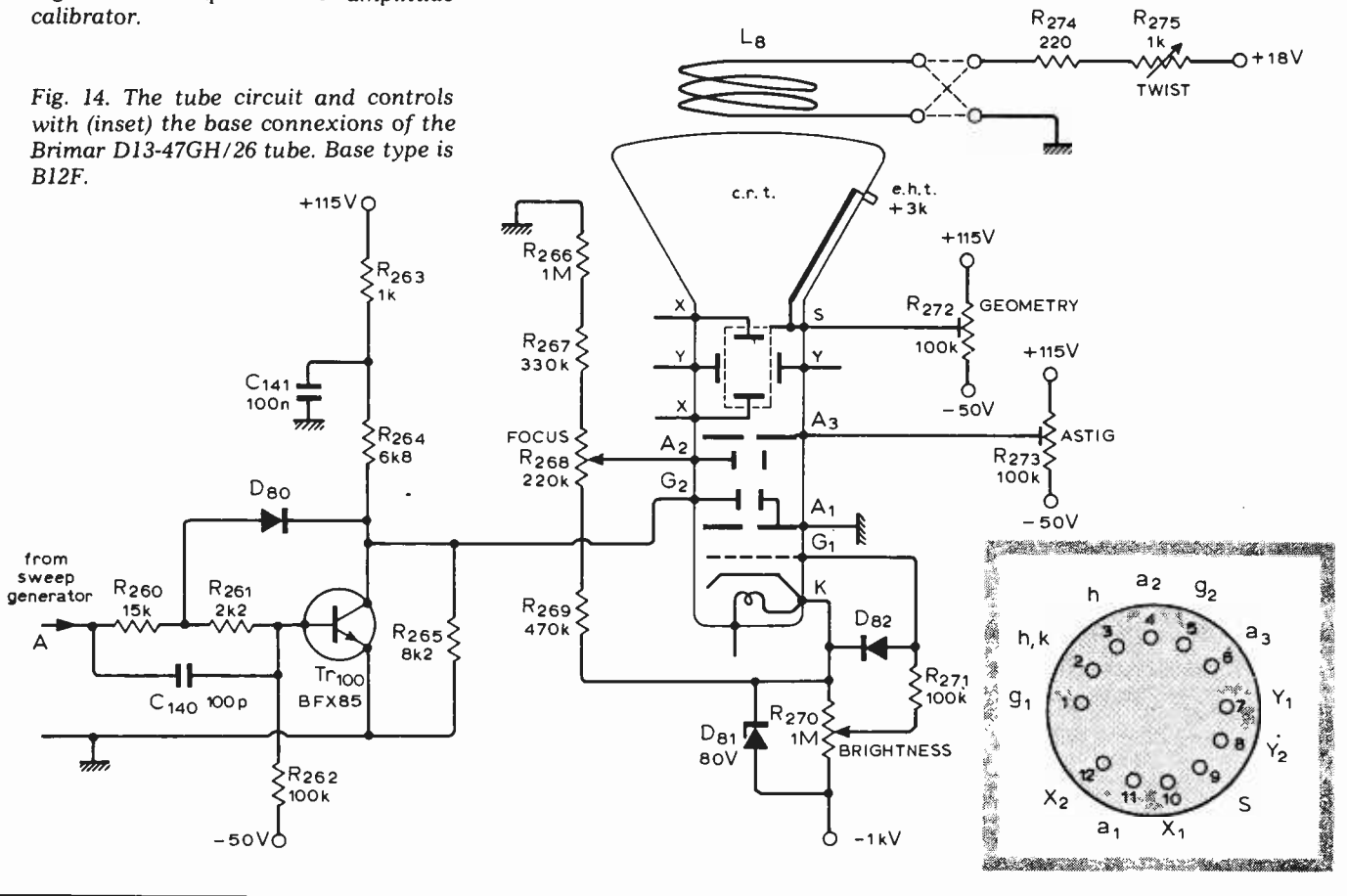


Fig. 13. The square-wave amplitude calibrator.

Fig. 14. The tube circuit and controls with (inset) the base connexions of the Brimar D13-47GH/26 tube. Base type is B12F.



Surplus p.d.a. tubes sometimes come on the market, and it is possible that a suitable one may be found. To aid bargain hunters, I have included, in Table 1, extracts from the manufacturers application data giving the main details of the c.r.t. The most important characteristics are the X and Y plate sensitivities, and it is necessary to use a tube with, at worst, sensitivities of 2/3 of these figures. If this is not adhered to, complete redesign of the amplifiers will be necessary. E.h.t. and other voltages are not usually so critical. If a tube is found that does not possess a second grid for blanking, but

is otherwise satisfactory, a circuit similar to Fig. 15 may be used.

An additional winding on the e.h.t. transformer is used to provide a floating supply of about 1.2kV. This is used to add a sufficient negative voltage to the output of the blanking amplifier to come within the required range of brilliance control voltages on the grid. The blanking amplifier needs an additional inverting stage to maintain correct polarities. Apart from these ideas I can provide no other information on other c.r.t.s, and any constructor who tries some other tube must make his own decisions.

To return to Fig. 14,  $D_{81}$  provides a negative voltage of 80V w.r.t. the cathode for the brilliance control.  $D_{82}$  is a safety diode to ensure that the grid cannot go positive with respect to the cathode.  $L_8$  provides an axial magnetic field for alignment of the horizontal trace with the internal graticule.  $R_{275}$  adjusts the current in this coil, and the connections are reversed if the correction is in the wrong direction.

$Tr_{100}$  is the blanking amplifier and is an unsaturated switch, with  $D_{80}$  preventing saturation. The beam is unblanked when  $Tr_{100}$  is on and grid 2 on the c.r.t. is at the same potential as anode 1, i.e. 0 volts. About 60 volts is necessary to fully blank the trace.

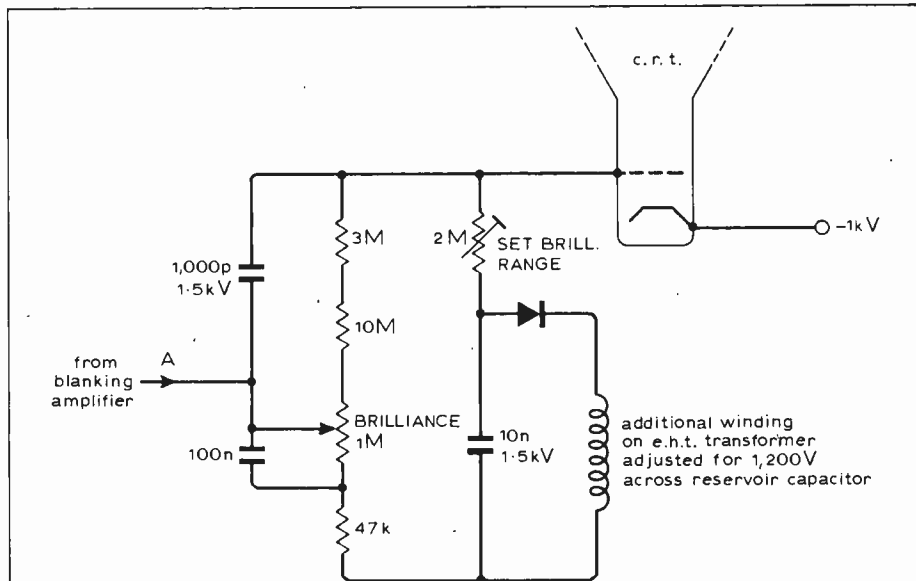


Fig. 15. Alternative grid drive when tube in use does not possess second grid.

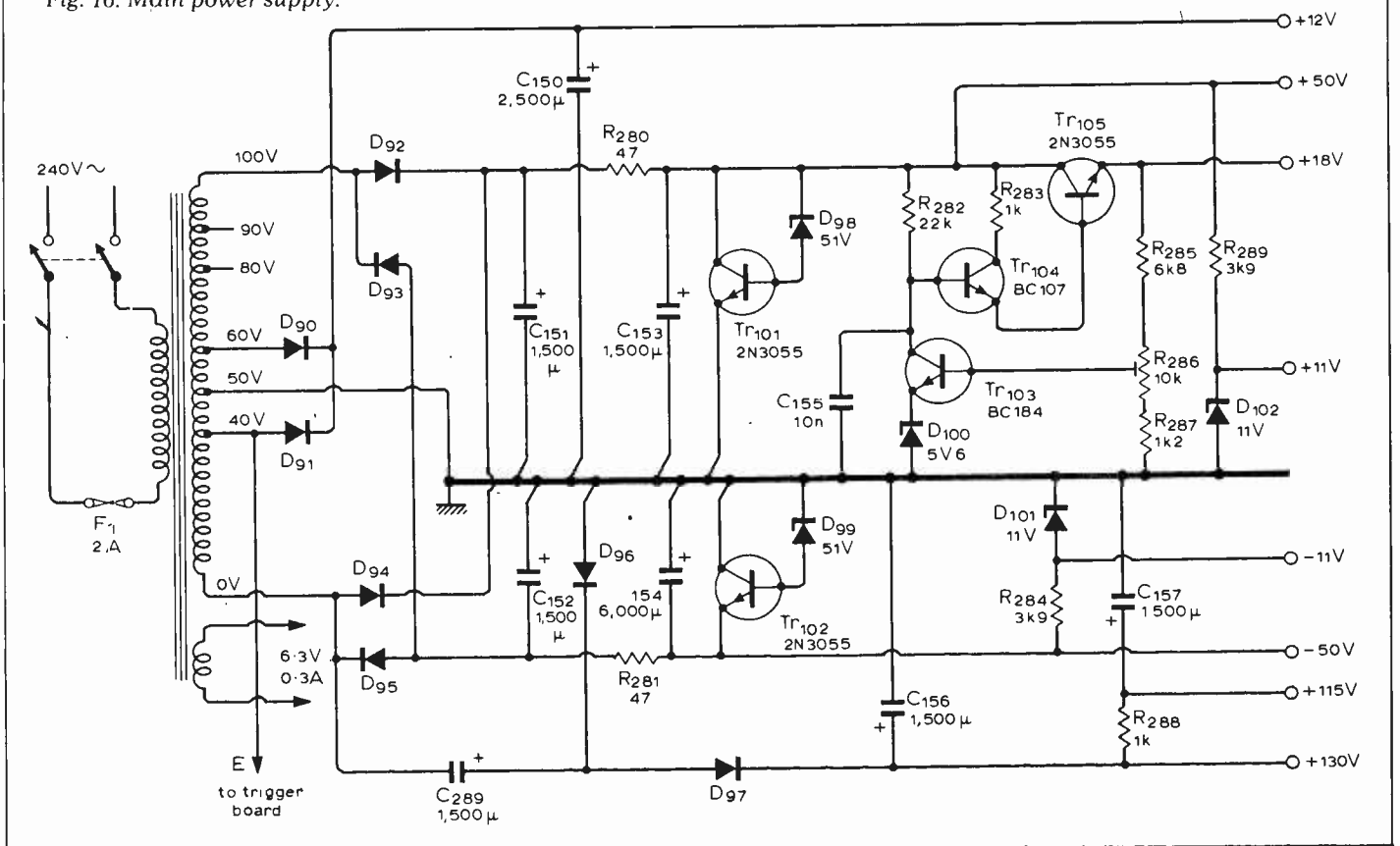
**Calibrator**

The amplitude and time calibrator is shown in Fig. 13. It is a conventional multivibrator which switches a constant current to and from a ladder attenuator. This provides a square wave of good rise and fall times with an amplitude that is independent of supply voltage variations.  $R_{241}$  and  $R_{244}$  enable the frequency to be set to 1kHz, and the mark-space ratio to unity.  $D_{73}$  provides temperature compensation for  $Tr_{92}$ .

**Power supply**

The mains power supply (Fig. 16) has been kept as simple as possible, consistent with a reasonable degree of stabilization. The main points are the large

Fig. 16. Main power supply.



number of different rail voltages needed, and the provision of a 6.3V, 0.3A a.c. supply for the c.r.t. heater. This winding floats at 1kV from earth. The +50 volt and -50 volt rails are derived from full-wave-rectified 70 volt unstabilized supplies by simple shunt stabilizers, which give adequate regulation and smoothing. The +18V rail is fed from a conventional negative-feedback stabilizer which uses the +50V line as its input. A preset,  $R_{286}$ , is used to set the rail voltage.  $R_{283}$  provides short circuit protection by limiting the drive current to  $Tr_{105}$ .

The X amplifier and the blanking amplifier need a higher voltage than 50V, in fact around 130V. This is obtained from a voltage doubler operating from one side of the 50-0-50 secondary on the transformer. The 130 volt rail is unstabilized. There is a fairly large amount of a.c. ripple on this rail, measured as 700mV peak to peak, and a dropping resistor  $R_{288}$  gives a smoothed voltage of +115V which is used in some of the circuits.

An unstabilized 12 volt supply feeds the e.h.t. generator, and finally a highly stable +11V and -11V for the shift controls is obtained from  $D_{102}$  and  $D_{101}$ .

The mains transformer is available from Osmabet Ltd, and its modification will be described in the section on construction.

**Table 1**

Some extracts from the manufacturers data on the c.r.t. type D13-47GH  
All voltages with respect to anode 1

4th anode (p.d.a.) voltage	+3kV
3rd anode voltage	-50V to +50V (astig)
2nd anode voltage	-600V to -825V (focus)
Cathode voltage	-1000V
Grid 1 volts for cut off	-1065V (brilliance)
Grid 2 volts for blanked trace	65 Volts
X plate sensitivity	14.5 to 17.5 V/cm
Y plate sensitivity	6.7 to 8.3 V/cm
Screen area	10x6cm

**Capacitances**

$X_1$ to $X_2$	2pF
$X_1$ to all less $X_2$	6.8pF
$X_2$ to all less $X_1$	6.8pF
$Y_1$ to $Y_2$	1.5pF
$Y_1$ to all less $Y_2$	6.4pF
$Y_2$ to all less $Y_1$	6.4pF

## Reference circuits — Circards 23

Set 23 of Circards, covering reference circuits, is now available. (Because of space limitations the introductory article has been omitted from this issue.) Titles in the set are

Reference circuits  
Zener diode characteristics  
Williams ring-of-two reference  
Variable reference diodes  
Bipolar references  
Low temperature coefficient voltage reference  
Voltage & current calibrator  
Compensated reference circuits  
Simple current reference  
Monolithic reference

### New circuit book

"Circuit designs — 1, Collected Circards" brings together the first ten sets of Circards, introductory articles to each of the subjects, and ten pages of additional circuits. The hardback A4 book contains 168 pages, in which 120 cards are rearranged so that each is laid out on one page. A brief introduction precedes the articles, which were previously published in *Wireless World*, and each of the ten subjects is followed by an up-dating page. Corrections have been incorporated where appropriate. "Circuit designs" is obtainable through leading bookstalls at £10 per copy. In case of difficulty order direct by sending remittance for £10.40 (includes postage and packing) to the address given later, making cheques payable to IPC Business Press Ltd. Advertisement appears on page 27.

Circards are a new method of collating and presenting data about circuits in a compact and easily retrievable way. The sets of 203x127mm (8x5in) double-sided cards are designed for easy filing in standard boxes and for easy access at the desk or at the bench, where transparent plastic wallets keep the cards in good condition.

Each card normally describes operation of a selected circuit, gives measured performance data and graphs, component values and ranges, circuit limitations and modifications to alter performance. Suggestions for further reading are included together with cross references to related circuits. The Circard concept was outlined more fully in the October 1972 issue of *Wireless World*, pp.469/70.

### How to get Circards

Order a subscription by sending £13.50 for a series of ten sets to:

Circards  
IPC Electrical-Electronic Press Ltd  
General Sales Department, Room 11  
Dorset House  
Stamford Street  
London SE1 9LU  
Specify which set your order should

start with, if not the current one. One set costs £1.50, postage included (all countries). Make cheques payable to IPC Business Press Ltd.

Topics covered so far in Circards are:

- 1 active filters
- 2 switching circuits (comparator and Schmitt circuits)
- 3 waveform generators
- 4 a.c. measurement
- 5 audio circuits (equalizers, tone controls, filters)
- 6 constant-current circuits
- 7 power amplifiers (classes A, B, C & D)
- 8 astable multivibrator circuits
- 9 optoelectronics: devices and uses
- 10 micropower circuits
- 11 basic logic gates
- 12 wideband amplifiers
- 13 alarm circuits
- 14 digital counters
- 15 pulse modulators
- 16 current-differencing amplifiers — signal processing
- 17 c.d.as—signal generation
- 18 c.d.as—measurement and detection
- 19 monostable circuits
- 20 transistor pairs
- 21 voltage to frequency converters
- 22 amplitude modulators.
- 23 reference circuits

## Hermetic plastics i.cs.

A process introduced by RCA is claimed to have overcome the problems of obtaining a hermetic seal in a plastic-packaged integrated circuit at no increase in cost. A high degree of hermeticity has previously been obtainable only with relatively expensive ceramic or glass packages and seals, the package bearing the brunt of atmospheric attack. In the new "trime-tal" process, the chip itself is sealed.

At the equivalent of the final oxide step in ordinary i.cs, a silicon nitride layer seals the junctions, a mask being used to gain access to contacts. Platinum is then sputtered over the wafer and sintered locally to provide platinum silicide. Layers of titanium and platinum are now laid down, the platinum layer being etched to provide interconnections, which are then gold-plated. (Titanium is used to provide an easy bond between platinum and silicon nitride.) All this avoids the use of aluminium interconnecting runs, which are prone to attack by moisture. The new process is applied to six RCA linear i.cs, including the CA741G and 747G which take the name of "Gold Chip" devices.

# Electronic circuit calculations simplified

## 2 — Resistive circuits (continued)

by S. W. Amos, B.Sc., M.I.E.E.

**Two resistors in parallel.** Every experimenter knows that the effective value of a resistor is reduced by connecting another resistor in parallel with it. But by how much is it reduced? To find out we can, of course, use the following well-known expression for the resistance of two resistors ( $R_1$  and  $R_2$ ) connected in parallel:

$$\text{effective resistance } (R_{eff}) = \frac{R_1 R_2}{R_1 + R_2}$$

$$= \frac{\text{product of individual resistances}}{\text{sum of individual resistances}}$$

As an example a 33-kilohm resistor in parallel with a 47-kilohm resistor has an effective value given by:

$$R_{eff} = \frac{33k \times 47k}{33k + 47k} = 19.4 \text{ kilohms}$$

In practice, however, problems concerning resistors in parallel are usually presented differently. Often we need to know what value of resistor must be connected in parallel with a given resistor to obtain a desired lower value of resistance. It is tedious and unnecessary to repeat the above calculation several times in order to obtain the answer. Instead the above expression can be rearranged as shown below to give the required information directly:

$$\text{resistor to be added } (R_2) = \frac{R_1 R_{eff}}{R_1 - R_{eff}}$$

$$= \frac{\text{product of original and effective resistances}}{\text{difference of original and effective resistances}}$$

As an example, if it is desired to reduce a resistor of 27 kilohms effectively to 22 kilohms, the resistance which must be connected in parallel is given by:

$$R_2 = \frac{27k \times 22k}{27k - 22k} = 120 \text{ kilohms}$$

The above expressions show that the value of a resistor is effectively halved by connecting an equal-value resistor in parallel with it. If the added resistor has twice the value of the original resistor, the net resistance is two thirds that of

the original resistor. If the added resistor has three times the resistance of the original, the net resistance is three quarters that of the original. In general if a resistor with  $n$  times the resistance of the original resistor is connected across the original, the net resistance is  $n/(n + 1)$  that of the original resistor.

Another useful rule which can be deduced from the above expressions is that in order to reduce the effective value of a resistor by 10%, the parallel resistor must have a value 9 times that of the original. For a 5% reduction, the parallel resistance must have 19 times the resistance of the original and for a 1% reduction the parallel resistance must be 99 times the original resistance. These added resistances are respectively approximately 10 times, 20 times and 100 times the original resistance — in each case 100 times the reciprocal of the percentage reduction required. Thus to effect a 2.5% reduction, the added resistance should be  $100/2.5$  i.e. 40 times the original resistance. In general to

reduce the effective value of  $p\%$  the added resistance should have a value of  $(100 - p)/p$  times the original and if  $p$  is small compared with 100, it can be neglected in the numerator of the fraction so that the added resistance is approximately  $100/p$  as deduced from the numerical examples earlier.

**Current divider.** The current  $I$  which flows externally to a parallel combination of resistors divides between them in the inverse ratio of their resistances. Thus in Fig. 16 the current ( $I_1$ ) flowing in  $R_1$  is given by

$$I_1 = \frac{R_2}{R_1 + R_2} \cdot I$$

and  $I_2$ , the current in  $R_2$ , is given by

$$I_2 = \frac{R_1}{R_1 + R_2} \cdot I$$

It is useful to regard a parallel resistor combination as a current divider because such a combination is often used as the basic negative feedback circuit in a current amplifier, and this approach enables the resistor values needed to give a wanted value of current gain to be readily calculated. Alternatively it enables the current gain of an amplifier to be deduced from inspection of the resistor values used in the feedback circuit.

For example, in the simplified circuit diagram of Fig. 17,  $R_e$  and  $R_b$  are effectively in parallel, the current path through  $R_b$  being completed by the input resistance of  $Tr_1$  which is normally small compared with  $R_b$ . The emitter current of  $Tr_2$  splits at the junction of  $R_e$  and  $R_b$  and the fraction of it which is returned to  $Tr_1$  base as a negative feedback signal is, as shown by the above expressions, given by  $R_e/(R_e + R_b)$ . Normally  $R_b$  is large compared with  $R_e$  and the fraction is thus approximately  $R_e/R_b$ . The current gain of the amplifier is equal to the reciprocal of this fraction i.e.  $R_b/R_e$ . The values of  $R_e$  and  $R_b$  should thus be chosen to give the desired value of current gain. Now  $R_e$  is one of the components used for biasing  $Tr_2$  and this consideration imposes limitations on its value: a likely value

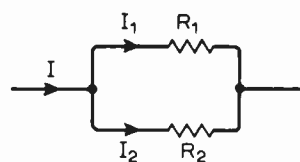


Fig. 16. Current division in a circuit composed of two resistors in parallel.

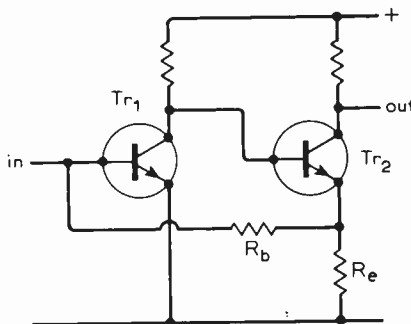


Fig. 17. Simplified diagram of a two-stage current amplifier in which gain is determined by the negative feedback circuit  $R_e R_b$ .

for  $R_e$  is 100 ohms.  $R_b$ , on the other hand, can be made almost any value and, to give a current gain of 100, should have a value of  $100 \times 100$  ohms i.e. 10 kilohms. Only the essential signal-frequency components are shown in Fig. 17: in a practical circuit additional components may be necessary, e.g. for stabilising the mean emitter currents of the transistors.

**Two resistors in series.** The effective value of two resistors  $R_1$  and  $R_2$  connected in series is the arithmetical sum of the two thus

$$R_{eff} = R_1 + R_2$$

Thus is a small resistor is connected in series with a large one, the effective resistance is slightly greater than the larger. (If the resistors are connected in parallel, of course, the effective resistance is slightly less than the smaller of the two.)

Two resistors connected in series are often regarded as a potential divider because the voltage  $V_{out}$  across  $R_2$  (Fig. 18) is a certain fraction of that ( $V_{in}$ ) applied to the combination: the fraction is determined by the resistor values according to the expression

$$V_{out} = \frac{R_2}{R_1 + R_2} \cdot V_{in}$$

which is similar to the expression for the current in  $R_1$  in a parallel resistor combination.

Potential dividers are often used for biasing transistors and Fig. 19 shows a typical circuit using an f.e.t. The potential divider  $R_1R_2$  impresses a particular value of voltage on the gate of the f.e.t. and the external source resistance  $R_s$  then determines the drain current of the transistor. This bias circuit is preferable to that in Fig. 3 (June) because it gives better d.c. stability i.e. it defines the mean drain current more accurately in spite of manufacturing spreads in transistor parameters and variations in parameters with temperature.

As mentioned earlier one of the features of f.e.t.s is that their input resistance is very high. Thus there is virtually no gate current and the resistors  $R_1$  and  $R_2$  are required solely to provide a particular voltage for the gate. The only current in  $R_1$  and  $R_2$  is therefore that which flows through them from the supply (the bleed current) and this can be made any desired value. Normally the bleed current is made very small because this enables the input resistance of the circuit to be kept high. To illustrate this let us assume that there is a 15-V supply and that the transistor is required to take 2mA mean drain (and therefore source) current. For such a current the transistor will be assumed to require a gate-source bias voltage of -1.5V. The gate voltage can be given any desired value up to 15V: 3V is a convenient

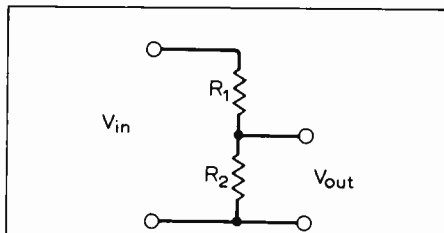


Fig. 18. Potential division in a circuit composed of two resistors in series.

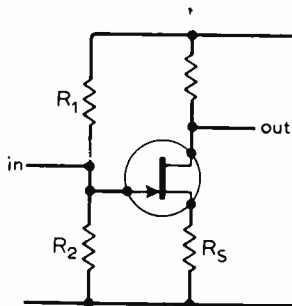


Fig. 19. Potential divider used to bias an f.e.t.

value. The mean source voltage must then be 4.5V to give the required gate-source bias. Thus the voltage across  $R_s$  is 4.5 and the current required in it is 2mA. Ohm's law gives the value of  $R_s$  as 2.2 kilohms.

The potential divider must give a gate voltage of 3 and the supply voltage is 15. Let us assume a very low value of bleed current, say  $10\mu A$ . This is then the current in  $R_2$  and the voltage across  $R_2$  is 3. Thus, from Ohm's law, the value of  $R_2$  is 300 kilohms. The current in  $R_1$  is also  $10\mu A$  and the voltage across it is 12 so that its value, also from Ohm's law, is 1.2 megohms.  $R_1$  is four times  $R_2$  and provided this ratio is maintained the gate voltage always has the same value of 3: the particular values chosen for  $R_1$  and  $R_2$  determine the bleed current.

In practice we are often concerned about the input resistance of the circuit. The input resistance of the f.e.t. itself is practically infinite but the input resistance of the circuit depends on  $R_1$  and  $R_2$ , which are effectively in parallel at signal frequencies. For the values of  $R_1$  and  $R_2$  calculated above the effective input resistance of the circuit is given by:

$$\text{input resistance} = \frac{\text{product of } R_1 \text{ and } R_2}{\text{sum of } R_1 \text{ and } R_2}$$

$$= \frac{1200k \times 300k}{1200k + 300k} = 240 \text{ kilohms}$$

With f.e.t.s it is possible to achieve much higher input resistances than this. For example, suppose we require an input resistance of 5 megohms: such a value might be required to terminate a capacitor or piezo-electric microphone or pickup cartridge. A useful way of calculating the values of  $R_1$  and  $R_2$  to give this value of input resistance as well as the required value of gate voltage is as follows. Let the ratio of the

gate voltage to supply voltage be  $a$ . This  $a$  is also therefore the step-down voltage ratio of the potential divider. Then the resistor values to use in the potential divider are given by:

$$R_1 = \frac{\text{input resistance}}{a}$$

and 
$$R_2 = \frac{\text{input resistance}}{1-a}$$

For the example in question  $a = 3/15 = 0.2$

$$\therefore R_1 = \frac{5}{0.2} = 25 \text{ megohms}$$

$$\therefore R_2 = \frac{5}{1-0.2} = 6.25 \text{ megohms.}$$

$R_1$  is four times  $R_2$  which ensures the required gate voltage. A calculation of the resistance  $R_1$  and  $R_2$  in parallel shows that this is 5 megohms as required.

The circuit of Fig.19 is also used to bias bipolar transistors but the design usually proceeds along entirely different lines from those described for f.e.t.s. This is primarily because the bipolar transistor has a significant input (base) current: as a result the input resistance is low and, because this shunts both resistors of the potential divider, there is no point in using high-resistance components for  $R_1$  and  $R_2$ . Indeed there is a good reason for using low-value resistors, namely that d.c. stability of the circuit is dependent on the value of these resistors, increasing as the resistor value is decreased. The resistors should therefore be made as low as possible subject to keeping the bleed current acceptable: in battery-operated equipment the potential divider should preferably not take as much current as the transistor itself.

A good starting point for the design is thus to decide on a value for the bleed current. Suppose the transistor is to take 1mA mean collector current. Then it is reasonable to let the potential divider take  $0.1mA$ . Let the required base voltage be 3V as before. Then a simple application of Ohm's law tells us that  $R_2 = 3/(0.1 \times 10^{-3}) = 30$  kilohms. Now  $R_1$  carries the base current of the transistor in addition to the bleed current of  $0.1mA$ . We can take the base current as  $1/\beta$  of the collector current. If  $\beta$  is 100 then the base current is  $0.01mA$  and the total current in  $R_1$  is  $0.11mA$ . If the supply voltage is 12 then there are 9V across  $R_1$  and the value of  $R_1$  is, from Ohm's law,  $9/(0.11 \times 10^{-3})$  i.e. 82 kilohms.

Finally we need to calculate the emitter resistor value. If the transistor is a germanium type the emitter potential is very nearly equal to the base potential and there is thus 3V across  $R_e$ . Since the current in  $R_e$  is 1mA, the value of  $R_e$  is given by  $3/(1 \times 10^{-3}) = 3$  kilohms. If, however, the transistor is a silicon type there is an offset voltage of approximately 0.7V between base and



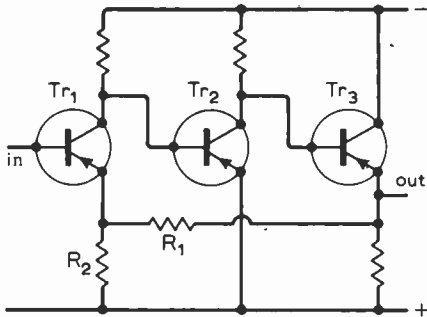


Fig. 20. Simplified diagram of a two-stage voltage amplifier with emitter follower output in which the gain is determined by the negative feedback circuit  $R_1 R_2$

emitter potentials and the voltage across the emitter resistor is only 2.3V, giving  $R_e$  as 2.3 kilohms.

If the base current had been ignored  $R_1$  would have been calculated as 90 kilohms instead of 81 kilohms. The difference is not great and to obtain approximate estimates of resistor values it is often permissible to neglect the base current.

A potential divider is often used as the basic element in the negative feedback circuit of a voltage amplifier and the values of the two resistors enable the gain of the amplifier to be set at a particular wanted value. Alternatively the gain of a voltage amplifier can be deduced from the values of the resistors in the negative feedback circuit. For example, in the simplified circuit diagram of Fig. 20  $Tr_1$  and  $Tr_2$  are common-emitter stages and  $Tr_3$  is an emitter-follower stage which provides the amplifier with a low output resistance.  $R_1$  and  $R_2$  constitute the potential divider which defines the voltage gain of the amplifier. The step-down voltage ratio of the potential divider is  $R_2/(R_1+R_2)$  but  $R_1$  is usually large compared with  $R_2$  and the step-down ratio is therefore approximately  $R_2/R_1$ . The voltage gain of the amplifier is equal to the reciprocal of this i.e.  $R_1/R_2$ . Thus if voltage gain of 200 is required  $R_1$  must equal  $200R_2$ .  $R_2$  is used to provide bias for  $Tr_1$  and its value is to a large extent determined by this consideration: a likely value for  $R_2$  is 100 ohms.  $R_1$ , on the other hand, can be given almost any value and, to give the desired value of voltage gain, should be  $200 \times 100$  i.e. 20 kilohms.

Only the essential signal-frequency components are shown in this circuit diagram: in a practical circuit additional components are necessary, e.g. for stabilising the mean collector currents of the transistors.

(Next article: capacitive circuits)

## Announcements

A one day conference in Cynenergetics is being organized at Chelsea College, University of London, by the Cybernetics Society on September 1st, 1975. Topics will include artificial intelligence, pattern recognition, cybernetic medicine, systems theory and other topics relating to cybernetics. Further details about the conference or offers of papers can be obtained from the conference organizers: E. Insam, c/o The Cybernetics Society, Chelsea College, University of London, Pulton Place, London S.W.6 or Dr. C. M. Elstob, Cybernetics Dept., Brunel University, Uxbridge, Middlesex. The Society also holds monthly meetings in London with speakers from various fields in cybernetics and other related topics, anyone interested in attending the meetings or becoming a member of the Society should contact Mr Kevin Clifton at the Cybernetics Society address or by telephone, 01-736 1244, ext 229.

**Norse Audio Systems Ltd** recently launched the Radionette range of audio and television equipment in the UK. The range, which is manufactured in Norway, includes colour television receivers, music centres, tuner-amplifiers, record decks, speakers, and transistor radios. Radionette (a subsidiary of the Tandberg organization) have said that the product range will be backed-up by a first-class after sales service.

Agreement has been reached to house the **Vintage Wireless Museum** of the Wireless Preservation Society in one of the Isle of Wight's "Stately Homes" — Arreton Manor, the home of Count and Countess Slade de Pomeroy. Arreton Manor already houses a Folk Museum, and a unique collection of dolls and dolls' houses.

**Dieter Assmann Electronics Ltd**, of Watford, manufacturers of a very wide range of components for printed circuit board assembly, have appointed Giltech Components of 22 Portman Road, Reading, as their first distributor in the U.K. Initially, Giltech will hold stocks of the major Assmann lines such as i.c. and transistor sockets, terminals, connectors and heat sinks.

**G. A. Stanley Palmer Ltd**, Elmbridge Works, Island Farm Avenue, West Molesey Trading Estate, Surrey KT8 0UR, have been appointed exclusive U.K. representatives for the National Wire and Cable Corporation of Los Angeles, California. Products manufactured include connecting wire both screened and unscreened, microminiature low voltage instrument control cable in single or pairs, under water cables, ultra flexible wires, multiple (single and pair) signal and control cables, and digital data transmission cables.

**Double R Electronics Ltd.**, Angus House, 13 Tilehouse Street, Hitchin, Herts SG5 2DU, have been appointed U.K. distributors for Ampower Semi-conductor Corporation in the United Kingdom.

## Vision network switcher

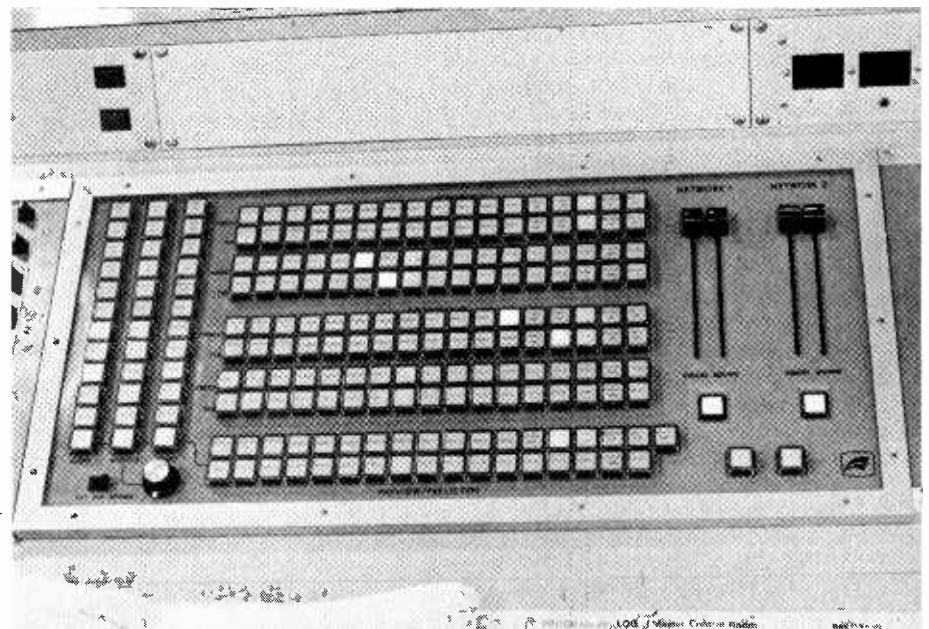
Logic-controlled network-switching equipment, recently installed at Yorkshire Television's Leeds studios, provides very simple routing of signals from 34 inputs (studios, telecine, v.t.r., etc) to three main external outputs and several internal monitoring and recording stations.

The photograph shows the control panel of the switcher, which contains the relevant buttons for two of the external outputs, the other being on another panel. The top two banks (of 68 buttons) each consist of 34 buttons to select signal source, coupled with "on air" lamps. When switching codes, set up in memory by the selector buttons, are activated by output "take" buttons, the "on air" lamps illuminate. Outputs

are to the Emley Moor YTV transmitter, the national network and the YTV Belmont transmitter, the selectors for this being on a separate panel. The bottom bank of buttons select inputs for previewing or prelistening and the left-hand set controls feeds to internal monitoring stations, etc.

In essence, the control panel sets up in memory the switching configuration required, resulting logic states being used to control single-f.e.t. cross-point switches (reeds, in the case of audio cross-points).

The equipment was supplied by Crow of Reading, the cross-points originating with Sandar Electronics — a Norwegian company.



# Noise — confusion in more ways than one

## 4—Noise figure and the design of front-ends

by K. L. Smith  
University of Kent at Canterbury

**The quest for low equipment noise temperature has formed a large part of research and development effort in recent times. The maser, parametric amplifier and other aspects of low-noise technique are covered in this concluding article. Noise figure is still commonly used to characterise performance and this idea, together with the earlier discussion of noise temperature, is considered to show that basically they are saying the same thing.**

Getting noise levels down at the front end of modern equipment has been a success story. In this section I will present an outline of some of the strides that have been made, but will not attempt a detailed description of actual front-end hardware, or specific devices and techniques. If you have any special interest requiring a little more detail, I have mentioned a few references for you to follow up.

The basic mechanism of noise generation in active devices is the shot effect, found, of course, in semiconductors as well as in thermionic emission devices. A serious limitation in microwave receivers has been the crystal mixer. Until the advent of low-noise r.f. stages such as the ruby maser and parametric amplifier, the crystal mixer was the front-end component. The crystal has a direct current flowing when operating and therefore shot noise is produced. This makes it appear "hotter" than an equivalent resistor under the same conditions. It also has a conversion loss. If you glance at equation 9 (Part 3), with  $L$  now standing for the mixer conversion loss and  $T_L$  somewhat above room temperature and related to the crystal noise temperature, then you will see that crystal mixers do not enhance the requirement for low effective input noise temperatures or microwave receivers.

One awkward point arises because of a traditional definition. The crystal noise temperature,  $T_x$ , is defined as the effective temperature at the output of the mixer stage when the input is terminated with a matched source resistor at  $T_0$  (290K). So  $T_x$  includes the source contribution at  $T_0$ . From this, taking care to account for the source contribution, we can write down an analogous equation to (9) for the  $T_e$  of the superhet with a crystal mixer front end and an i.f. amplifier whose effective

input noise temperature is  $T_{i.f.}$

$$T_e = LT_x - T_0 + LT_{i.f.} \quad (11)$$

The first term is the crystal noise temperature referred to the front end or input terminals; the second term is the subtraction of the standard source temperature, assumed in the definition of  $T_x$ ; and the third term is the i.f. amplifier input temperature referred forward to the front-end terminals. For good noise performance, a low  $T_x$  and small  $L$  is required. A manufacturer's catalogue shows the following for the 1N23C point-contact X-band mixer diode:  $t_x (= T_x/290) = 2, L = 6\text{dB}$ , which is a loss of four times.

Putting these values into (11) gives

$$T_e = 4 \times 2 \times 290 - 290 + 4 \times 116 \approx 2500\text{K}.$$

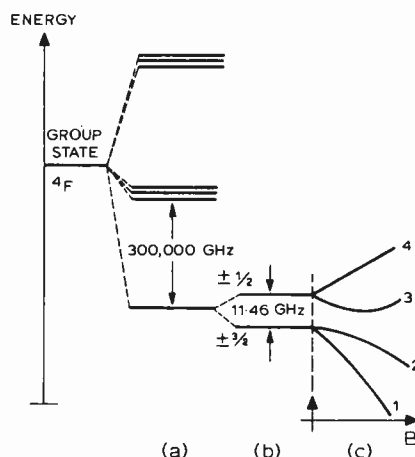


Fig. 16. Quantum mechanics explains the pattern of energy levels obtained in crystal lattice structures (among other things). Example shown is for chromium ions in ruby crystals. Altering value of the magnetic flux  $B$ , sets the levels 1, 2, 3 and 4 at convenient energy intervals for maser action.

I have assumed a low-noise i.f. amplifier, a temperature of  $T_{i.f.} = 116\text{K}$ . The noise temperature of 2500K is not a very good performance. From the same catalogue, a modern Schottky-barrier mixer diode type P1906F would give an effective input noise temperature of 740K if used in the same receiver.

Other hazards exist which I have ignored in the above discussion. An important one is the noise generated in the local oscillator. The noise sidebands from the oscillator mix to produce an appreciable output at the i.f. frequency. A balanced mixer should be used to reduce noise from this source. Another dodge is to lock the local oscillator to a low-noise stable frequency generator, such as a crystal oscillator and multiplier chain (which, incidentally, reduces the drift, frequency jumping and the f.m. noise of the local oscillator). The noise performance of the i.f. amplifier is critical with direct conversion receivers. The presence of the loss factor  $L$  makes this so, as you can see from (11).

The first stages of the amplifier require transistors specially selected for their good noise performance and the optimum matching conditions between mixer and i.f. input circuit is important. It is possible to obtain optimum performance empirically by switching on and off a gas-tube noise source coupled into the front end, attenuated if necessary, while adjusting the mixer, local oscillator, and i.f. couplings for minimum  $T_e$ , as monitored by observing the changes on a power meter at the output of the system. The calculation of the optimum conditions for any given case, including the effects of parasitic reactance, etc, is extremely difficult. If you wish to follow this up, E. G. Nielsen<sup>14</sup> wrote an interesting article on the topic.

You may recall the publicity, about a decade ago, in connection with the Goonhilly station system. The "signifi-

cant" results that the new maser amplifier was going to make possible were indeed achieved, after the usual teething troubles. We had visions of large Dewar flasks surrounded by liquid-nitrogen-produced vapour clouds and all the other complexities of the cryogenics. The cost and complexity of the maser hardware and cryogenics, and the relatively narrow bandwidth obtainable has meant a decline in their use, and the much more convenient parametric amplifier has taken over. In spite of this, the maser still offers the ultimate in low-noise performance, because not only are the "working bits-n-pieces" cooled to about 4K with liquid helium, you will sometimes see negative temperatures mentioned! Of course, the physical temperature is never below absolute zero, but in some ways the maser acts as if it were.

The action of the solid-state maser depends on materials with paramagnetic ions in a crystal lattice, such as the chromium<sup>3+</sup> ion in ruby. The spin and orbital motion in these atomic particles are quantized, which means that the only energies allowed them by the laws of quantum physics are very definite values. Any change in energy of particles means a jump from one energy level to another with the absorption or emission of radiation of characteristic frequency. This is pictured in a diagram such as that in Fig. 16; (a) shows some of the chromium ion levels in ruby. The lowest level is the only one of interest for maser work.

In this ion, there are three available electrons which contribute to the paramagnetic splitting. The three electrons give four possible energy levels and the fields of force in the crystal lattice split the levels into two pairs 11.46-GHz apart (the energy difference is measured in "frequency" - this being the frequency of the radiation involved in any jump between the levels), see Fig. 16 (b). A long time ago a fellow named Zeeman in 1896 found that applying an external magnetic field to atoms or molecules with levels which have the same energy (the jargon for this is that they are "degenerate", but this does not mean that they suffer from anything nasty!) separates them, or as we say lifts

the degeneracy by an amount depending on how strong the magnetic field is.

Sure enough, this happens with our chromium ions in ruby, see Fig. 16 (c). The low energy levels of the billions of particles in the crystal lattice are occupied according to the quantum laws, and the absolute temperature  $T$ . The lowest levels are crowded while higher levels are only sparsely filled. The whole point of maser action is to invert this population distribution - by pumping, so that when dropping back to a low energy level, the electrons involved give energy to the passing signal wave, boosting its amplitude. The waves passing through the crystal (we are discussing a travelling-wave maser) need time to interact with the excited atoms, so a careful design is made of a slow wave structure for this purpose.

The correct populations can only be produced at very low temperatures - hence the liquid helium involved. The magnetic field to split the energy levels to just the right value for the frequency of the signal and pump is often applied by the use of a "persistent current superconducting magnet" - a case of exploiting the very low temperature available and the resulting superconductivity in some materials. Fig. 17 (a) illustrates this and (b) shows diagrammatically the parts of the travelling-wave maser.

We can sum up all of this by noting that the signal wave in a maser extracts energy in phase from the excited ions in

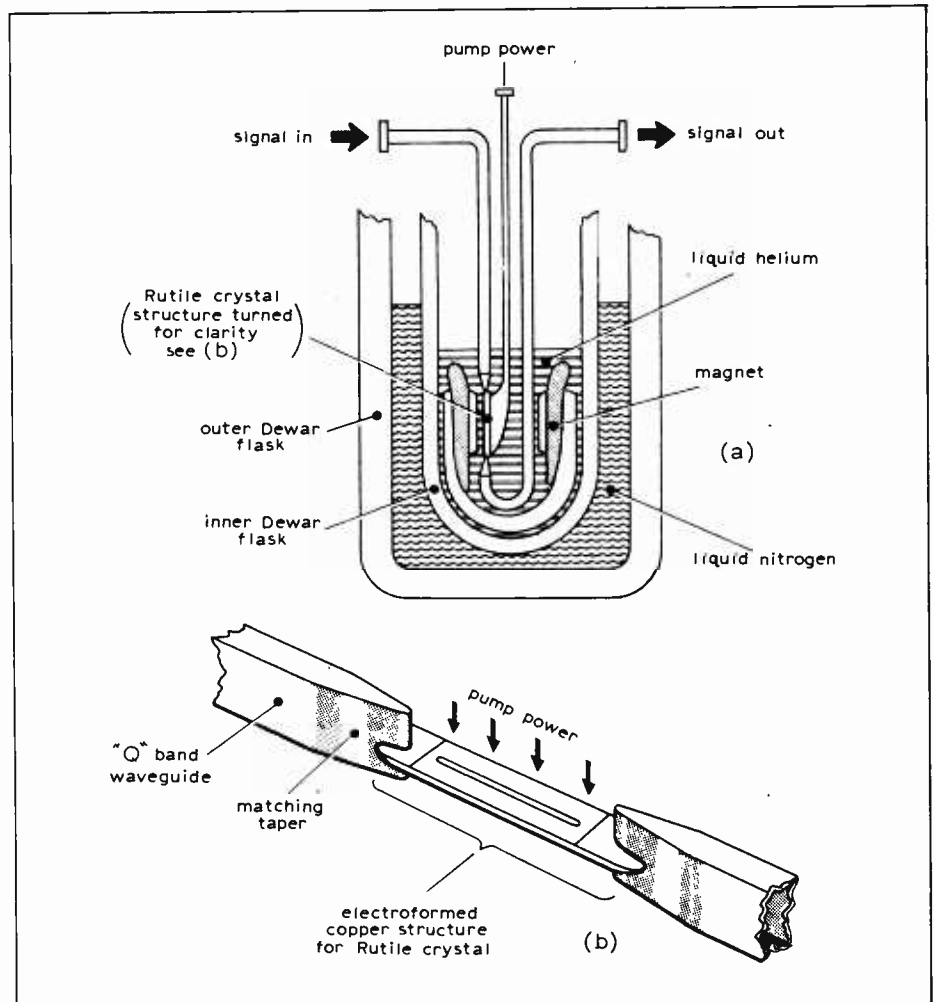
the crystal. The presence of the signal stimulates the emission - hence the name of the device, Microwave Amplification by Stimulated Emission of Radiation, as you probably already know. The extremely low effective noise temperature of this amplifying mechanism arises from the requirement to use liquid helium temperature, together with a further reduction of this already low temperature according to  $T_{e(maser)} = T_{amb}/I$ , where  $T_{amb} \approx 4.2K$  (liquid helium) and  $I$  is the inversion ratio of the maser, usually about three and is the number of times the upper energy level is more densely populated than the lower, as a result of the pumping action.

Naturally, the signal has to be got into the amplifying part of the maser, and out again. Equation 9 shows that the effect of any attenuation in the feeder at the input, will very convincingly degrade the noise performance.

$$T_e = (L-1)T_L + \frac{LT_{amb}}{I} \quad (12)$$

If  $T_L$  is a mean temperature of around 100K and  $L$  is a loss of only 0.5dB (1.12 times), then  $T_e = (1.12 + 56)K$ . That is, the loss contributes about 11K and the maser itself about 1.5K. Herein lies a big difficulty with such amplifiers: how to get the signal down into the crystal in the Dewar, through the couplings and hardware of the front-end feeder system, without introducing prohibitive losses. Taking the signal out is all right, it has been amplified by the maser gain,

Fig. 17. Inconvenience of maser amplifiers is mainly because of the complex cryogenic system required. Also, getting the signal in and out and the pump power in to the crystal is troublesome. Shown here is a typical example of a maser with rutile for the slow-wave structure and in interacting element (a). Magnet could be a self-sustaining superconducting one. Velocity of the wave in rutile is very much less than the velocity in free space, because of the high dielectric constant. One method of feeding in the pump power that has been proposed is to use a side radiating horn, as shown at (b). (A. Fletcher).



perhaps 45dB or so. A good article on masers was presented in *Philips Technical Review* in 1965 if you can get hold of a copy<sup>15</sup>. The practical description of the Goonhilly Down maser is discussed fully.

**Parametric amplifier**

The source of gain in the parametric amplifier is an entirely different physical mechanism to that in the maser system, although a pump oscillator is again employed. Most of the literature proudly states that Lord Rayleigh, and even Michael Faraday, spoke of the paramp principle way back in the last century. This is so, but the electronic realization of the principle for low-noise amplification is recent (the 1950s). Basically a reactive parameter, such as a capacitance, is varied and this feeds energy into a signal wave. Being a virtually noiseless parameter (reactance), the usual Johnson and current noise contributions are reduced. There is some loss in the active device, which is usually a varactor diode, and in the feeder hardware. Cooling will therefore lower the effective noise temperature. Noise contributions also arrive in the pump frequency oscillations and can degrade the performance.

Three frequencies are usually involved in a paramp; the signal frequency  $f_s$ , the pump  $f_p$  and the idler frequency  $f_i$ . The idler frequency is the mixing product of  $f_s$  and  $f_p$ , i.e.  $f_i = f_p - f_s$ . Much of the design work in parametric amplifier projects is involved with the correct design of the resonant structures for  $f_s$  and  $f_i$  and in ensuring the isolation between them. A circulator is required at the signal front end, because the varactor diode is a two-terminal device. (Tunnel diode amplifiers also have this drawback.) You are correct if you immediately assumed that isolators, circulators, switches or any other such lossy hardware in the input feeder are bad for low-noise performance, equation 9 or 12 operates again.

Fig. 18 gives some idea of the electrical arrangement of a pumped paramp of the "two-tank" variety. The input signal arriving at port 1 of the circulator is diverted out of port 2 into the signal-tuned circuit  $CL_s$  in the paramp. The pump is, varying the capacitance of the varactor and energy is fed into the signal oscillations by this action. The amplified signal is passed back to port 2 of the circulator. (You could look upon all this as a signal passing into the paramp on the input transmission line and there reflected with a reflection coefficient greater than unity back down the line.) The circulator passes the amplified signal out of port 3 to the load. The circuit  $CL_i$  resonates at the idler frequency and filters  $F_i$  and  $F_s$  reject the idler and signal frequencies respectively so keeping the various signals and oscillatory powers in their places.

There are various ways in which the realization of the scheme shown in Fig. 18 can be carried out. Fig. 19 shows just one possibility. The pump is much higher in frequency than the signal and is usually supplied via a waveguide, although microstrip techniques are increasingly being employed.

A theoretical analysis of Fig. 18 enables the gain, noise temperature and bandwidth of the amplifier to be derived. If you are interested in some of the theoretical argument, you will find a very good discussion in reference 16. One factor of great importance is  $\gamma$ , which is defined as

$$\frac{C_{max} - C_{min}}{2(C_{max} + C_{min})}$$

This is a kind of goodness factor for the varactor diode and indicates the amount of capacitance variation obtainable by pumping. Another diode parameter is the cut-off frequency,  $f_c = 1/2\pi CR_d$ , which must be way above the frequencies involved in the amplifier. Noise is contributed directly by the diode loss resistance  $R_d$  and also  $R_i$  in the idler circuit. It is in cooling these

that the improved performance at low frequencies is obtained. Quoting now the noise temperature expression (see reference 16)

$$T_e = T \left[ \frac{R_d}{R_g} + A \frac{f_s}{f_i} \left( 1 + \frac{R_d}{R_g} \right) \right]$$

where  $R_g/R_d$  is often called the over-coupling ratio and  $T$  is the physical temperature.  $A$  is dependent on the gain, but is normally close to unity, especially at high gain. This means that if we make  $R_g \gg R_d$ , then the effective noise temperature of the paramp is

$$T_e \approx T \frac{f_s}{f_i} \tag{13}$$

Under these conditions, we can see that if the pump frequency is high, so that  $f_s \ll f_i$  then the effective input noise temperature of the parametric amplifier can be made less than the physical temperature (i.e. by the fraction  $f_s/f_i$ ). Lest you think "Ah! let's push up the idler frequency to millions of gigahertz - and get noise temperatures around absolute zero", life is not so kind. Remember  $f_c$  for the diode, and other losses limit the possibility of an unlimited rise in the pump and therefore idler frequency. The noise temperature given by (13) is oversimplified and as the gain drops when  $f_p$  goes up the noise temperature will start to increase again. This would indicate that there is a minimum noise temperature for an optimized paramp with a given diode, packaging, and so on. It can be shown that

$$T_{e(min)} = \frac{2f_s}{\gamma f_c}$$

As would be expected, a large  $\gamma$  and high  $f_c$  for the diode is the best way to a low  $T_e$  at any given signal frequency  $f_s$ .

**Handling the idea of noise figures**

The noise figure,  $F$ , has already been mentioned and you may recall from part 1 that H. T. Friis and D. O. North were instrumental in getting the concept off the ground. All the equations to calculate  $F$ , are derived from the basic definitions in a similar way to the expressions for  $T_e$ . If we went through it all again, it would mean a duplication of effort. The main point now is to derive the relationship between  $F$  and  $T_e$  so that all the earlier equations can be written in terms of  $F$ , if required. Friis defined  $F$  as the signal-to-noise ratio at the input of a network when the source resistance is at 290°K; divided by the signal-to-noise ratio at the output of amplifiers, receivers and so on, are always smaller than those at the input, then  $F$  is always larger than one.

From the above verbal definition you will see that

$$F = \frac{S_i}{P_{Ni}} \bigg/ \frac{S_o}{P_{No}}, \text{ and this ties up to } \frac{S_i P_{No}}{P_{Ni} S_o}$$

If the network has a power gain of  $G_A$ ,

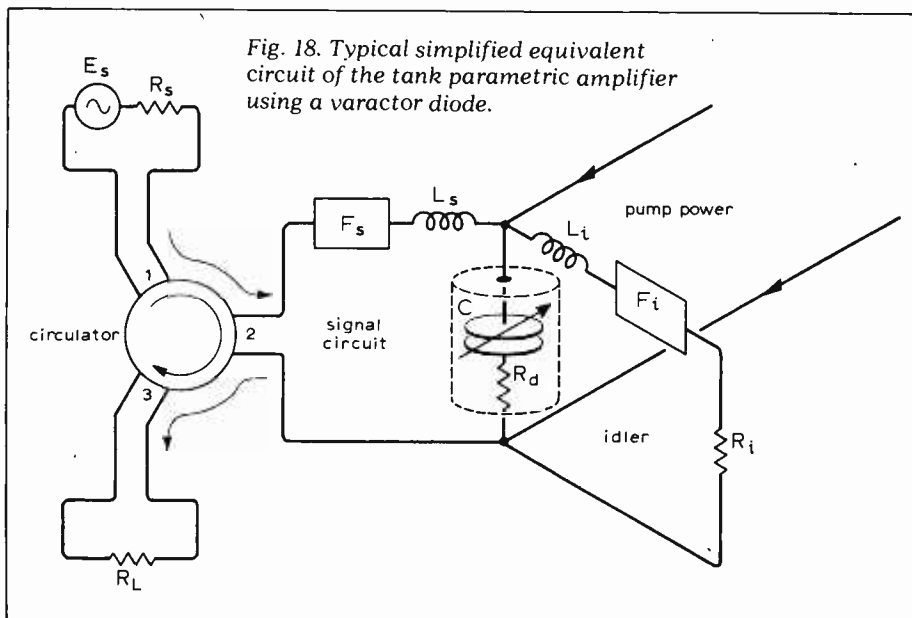


Fig. 18. Typical simplified equivalent circuit of the tank parametric amplifier using a varactor diode.

then  $S_o = G_A S_i$  and  $P_{No} = G_A P_{Ni} + P_{Na}$ , by precisely the same argument that was made in part 2 (first paragraph). This means that

$$F = \frac{S_i(G_A P_{Ni} + P_{Na})}{P_{Ni} G_A S_i} = 1 + \frac{P_{Na}}{G_A P_{Ni}} \quad (14)$$

Immediately from the equation  $P_{Na} = G_A k T_e B$ , (part 2) and  $P_{Ni} = k(290)B$ , so that from equation 14

$$F = 1 + \frac{T_e}{290} \quad (15)$$

This is the relationship connecting  $F$  and  $T_e$  we set out to find.

I indicated at the beginning of this series that D. O. North also defined a noise factor. His definition dispensed with signals right from the start. You may like to see that his definition is just the same as that just given in (15), although North originally suggested 300K for the standard temperature. North's definition went like this: "F is the ratio of the total noise power output from a system when its input termination is at 290K, to that part of the output which arises from the input termination only".

In symbols, this is

$$F = \frac{P_{No} \text{ (when } T_i \text{ is 290K)}}{G_A k(290)B}$$

but  $P_{No} = G_A k B(290 + T_e)$ , see part 2, p.169, and therefore

$$F = 1 + \frac{T_e}{290}, \text{ as before.}$$

Some early ideas connected with this topic was discussed in *Wireless World* by L. A. Moxon<sup>17</sup>.

We are now in a position to write down any noise expression in terms of  $F$  by using the fact that  $T_e = 290(F-1)$  by transposing (15). You can see this from the following examples.

Substituting for  $T_e$  in the equation on p.171 (part 2) gives

$$F = F_1 \frac{F_2 - 1}{G_i} + \frac{F_3 - 1}{G_1 G_2}$$

From equation 6

$$T_e = \frac{T_{hot} - A T_{cold}}{A - 1} \text{ or}$$

$$290(F - 1) = \frac{T_{hot} - A T_{cold}}{A - 1},$$

$$F = \frac{\frac{T_{hot}}{290} - A \frac{T_{cold}}{290}}{A - 1} + 1 \text{ which is}$$

$$F = \frac{\left(\frac{T_{hot}}{290} - 1\right) - A \left(\frac{T_{cold}}{290} - 1\right)}{A - 1}$$

The quantities in the brackets are excess noise ratios. Very often  $T_{cold} = 290K$ , so that

$$F = \frac{\frac{T_{hot}}{290} - 1}{A - 1}$$

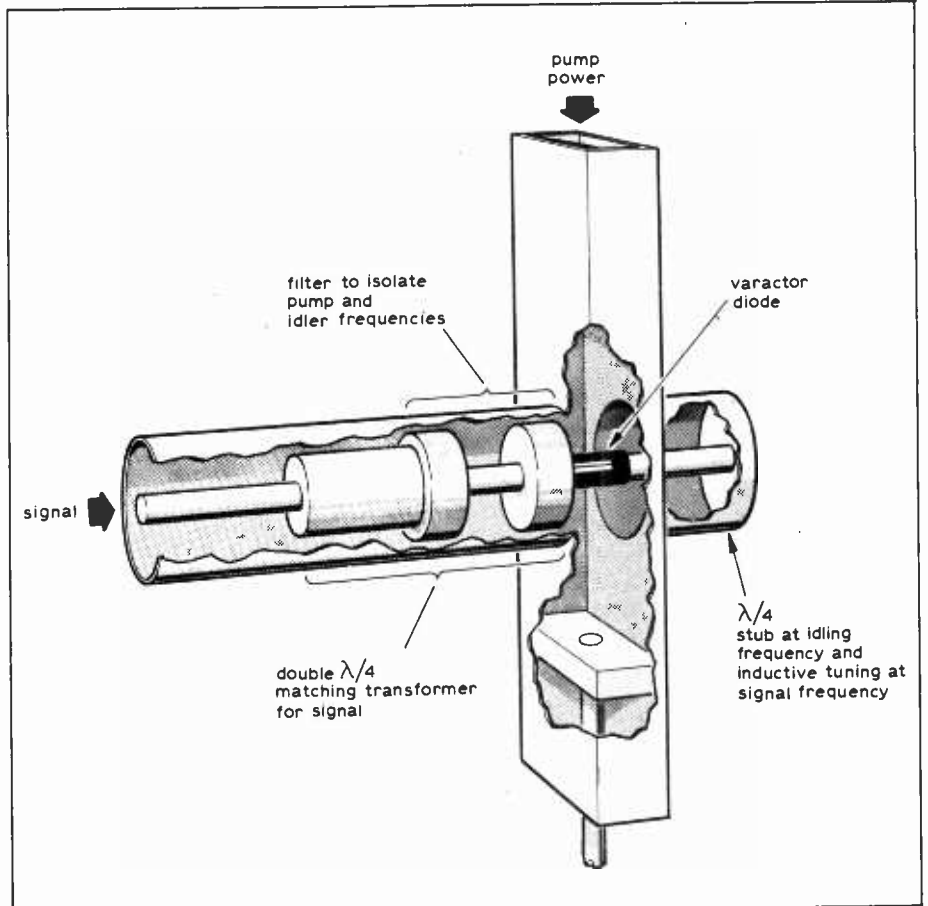
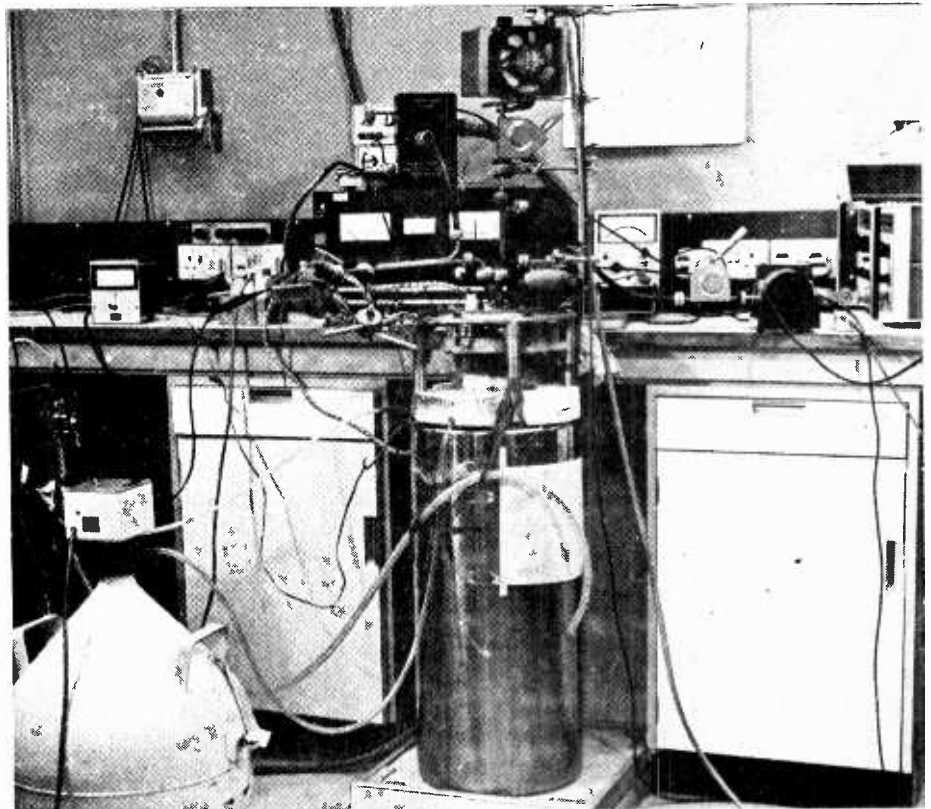


Fig. 19. Hardware of a parametric amplifier for the hundreds of megahertz to lower gigahertz region often consists of a mixture of coaxial and waveguide techniques. This illustration is based on a system described by Aitchison, Davies and Gibson of Mullard Research Labs.

View of Tony Fletcher's 35GHz maser at the University of Kent. Pump power is obtained from a klystron operation at 80GHz. The complexity of the cryogenics is obvious.





If  $A$  is made 2 by choosing the value of  $T_{hot}$  to make it so, then

$$F = \frac{T_{hot}}{290} - 1$$

The last equation in part 2 shows this to be equal to  $20I_a R$  for a noise diode, so that we have the interesting result  $F = 20I_a R$ , a well-known expression.

For the next example, we can look at (8), which when substituted gives

$$F = 1 + \frac{(L-1)T_L}{290}$$

Similarly from (9)

$$290(F-1) = (L-1)T_L + L(290[F_R-1])$$

$$F = 1 + (L-1)\frac{T_L}{290} + L(F_R-1)$$

Considering equation (11), we can now see why we had some argument about  $T_x$ , because the original derivations were in terms of  $F$ . We should expect to see a simplification when "going backwards" to  $F$ , to the well-known equation for crystal mixer performance. Now  $T_e = 290(F-1)$  and  $T_{if} = 290(F_{if}-1)$ , also  $T_0 = 290K$  all by definition, so that equation 11 gives

$$290(F-1) = LT_x - 290 + L290(F_{if}-1)$$

$$F = L(t_x + F_{if}-1)$$

where  $t_x = T_x/290$ . This is often seen quoted in discussions about crystal mixers.

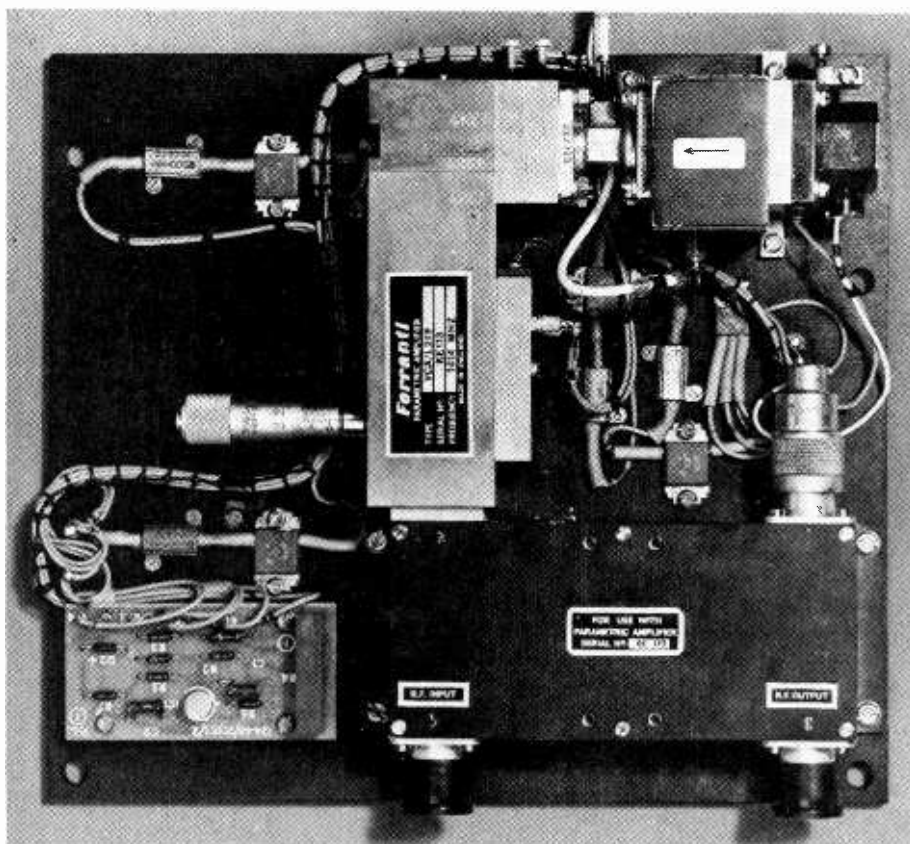
And so we could go on. Notice that there is often a "1" for the first term on the right-hand side in noise figure

equations. This arises because of the contribution of the source at 290K. When the division by 290 is made to obtain the ratio that is  $F$ , the first term is "1". This means (by subtracting the "1" from both sides) that the expression  $F-1$  occurs frequently, hence the growth of the term excess noise figure for this. Because I am making a case for a decline in the use of  $F$  and an increase in thinking in terms of temperature, I will not labour the point any further.

If you would like to give more prominence to  $F$ , and convert all the formulae, for instance, then you can go ahead. But, in this series of articles, I have attempted to show that the mysteries of "temperature" are only imaginary and that so long as care is taken to realise that the term has been extended to mean more than physical hotness, then the idea is valuable in noise discussions.

I suggest that the noise figure is not so clear as temperature, and is tied to "290K", which is sometimes manipulated behind the scenes for the unwary, and this makes a mockery of "F".  $F$  has

*This is a typical low-noise (50K) commercially-made parametric amplifier. Example illustrated operates at a signal frequency of 1414MHz. Coaxial circulator is seen at the bottom right and the pump power is obtained from the solid state oscillator at the bottom left, which feeds power to the varactor via a ferrite isolator. Amplifier was supplied to Cambridge University for radio astronomical observations around the hydrogen-line frequency. (Courtesy of Ferranti Ltd.)*



a habit of being what anyone wants it to be (see the satirical article The Art of Noisemanship by J. C. Green<sup>18</sup>, also The Noise Figure Muddle by Seymour B. Cohn<sup>19</sup>). As you might see, a lot of confusion can arise. If you have not yet embarked upon a course of advanced study in electronics, perhaps I have been able to give you an inkling of the interesting concepts concerning equipment limitations, meanings of temperature, etc, that you are likely to meet as part of your studies. If you are already doing some work in communications engineering, then a few of the points covered in these articles may show a little of what is "behind the scenes". Mastering the technique of handling  $T_e$ , and especially  $T_{op}$  or  $T_{sys}$  gives you a direct route to the overall signals-to-noise ratio - which when all is said and done, is the vital parameter in modern communications systems.

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**Correction to part 2 (April issue)**

An error occurred in the discussion of noise bandwidths in Appendix B, page 173. The two equations for  $G_A$  at the top of the page are correct, but  $L$  and  $C$  have subsequently become transposed. There is a symmetry about  $L$  and  $C$ , so the final result is correct, but the statement

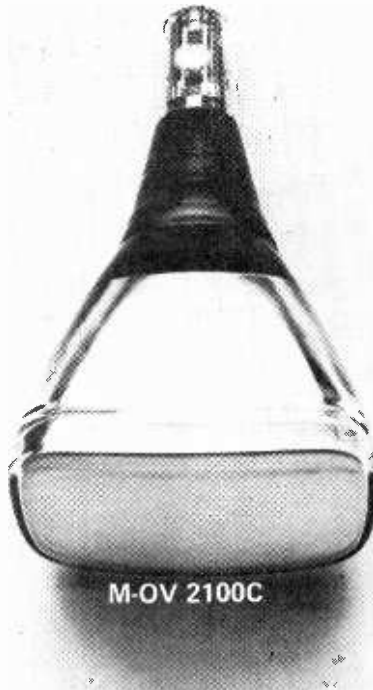
$$R = \omega C \frac{1}{\omega L} \text{ should read } R = \omega L \frac{1}{\omega C}$$

and all  $L$ s and  $C$ s should be interchanged from then on. (The error is obvious if you look at the statement  $B_{3dB} = R/2\pi C$ , which cannot be true because it is dimensionally incorrect. Replace  $C$  with  $L$  and it is then alright.)

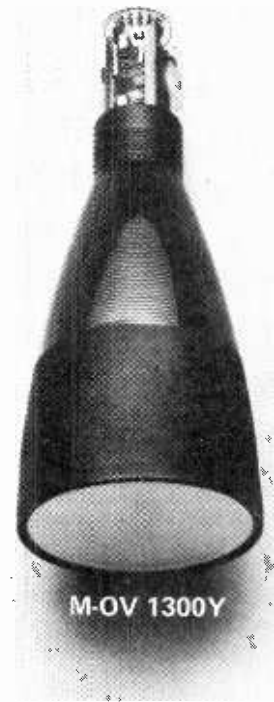
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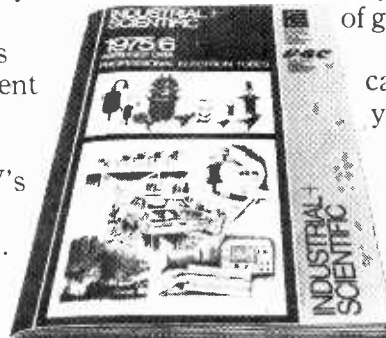
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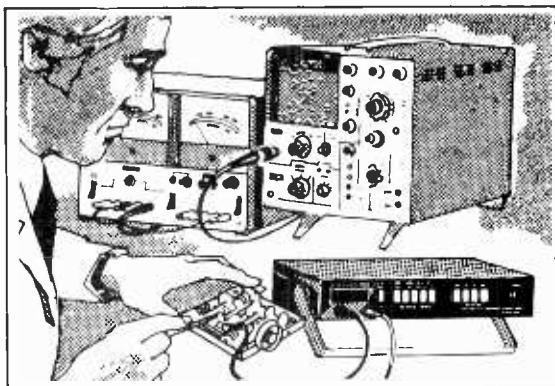
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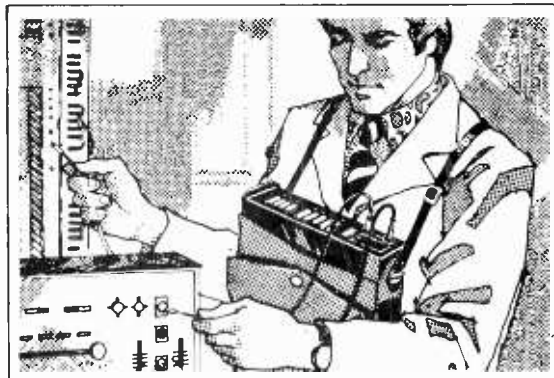
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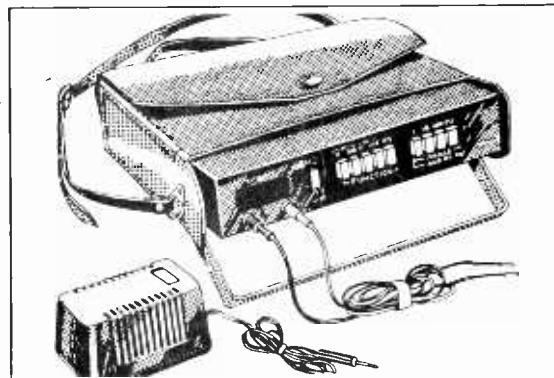
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1000 V	0.5% ± 1 "	10 MΩ	1 V

Maximum overload - 350 V on 1 V range  
1000 V on all other ranges.

AC Volts Range	Accuracy	Input Impedance	Frequency Range
1 V	1.0% ± 2 Digits	10 MΩ/40 pF	20 Hz-3 KHz
10 V	1.0% ± 2 "	10 MΩ/40 pF	20 Hz-3 KHz
100 V	2.0% ± 2 "	10 MΩ/40 pF	20 Hz-3 KHz
1000 V	2.0% ± 2 "	10 MΩ/40 pF	20 Hz-1 KHz

Maximum overload - 300 V on 1 V range  
500 V on all other ranges.

DC Current Range	Accuracy	Input Impedance	Resolution
100 μA	2.0% ± 1 Digit	10 KΩ	100 nA
1 mA	0.8% ± 1 "	1 KΩ	1 μA
10 mA	0.8% ± 1 "	100 Ω	10 μA
100 mA	0.8% ± 1 "	10 Ω	100 μA
1000 mA	2.0% ± 1 "	1 Ω	1 mA

Maximum overload - 1 A (fused).

AC Current Range	Accuracy	Frequency Range
1 mA	1.5% ± 2 Digits	20 Hz-1 KHz
10 mA	1.5% ± 2 "	20 Hz-1 KHz
100 mA	1.5% ± 2 "	20 Hz-1 KHz
1000 mA	2.0% ± 2 "	20 Hz-1 KHz

Maximum overload - 1 A (fused).

Resistance Range	Accuracy	Measuring Current
1 KΩ	1.0% ± 1 Digit	1 mA
10 KΩ	1.0% ± 1 "	100 μA
100 KΩ	1.0% ± 1 "	10 μA
1000 KΩ	1.0% ± 1 "	1 μA
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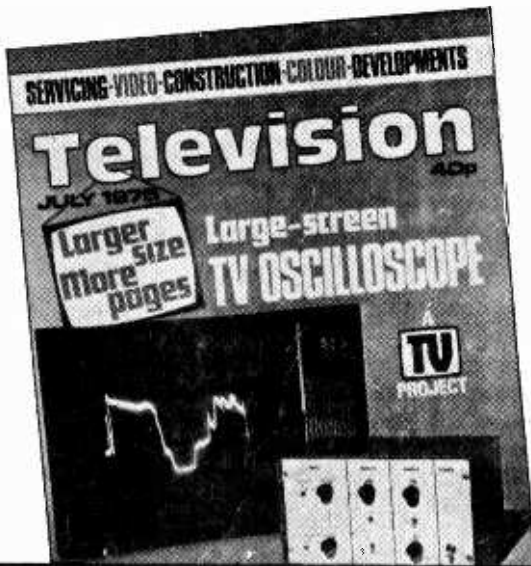
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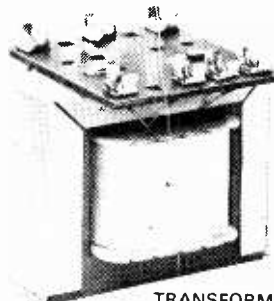
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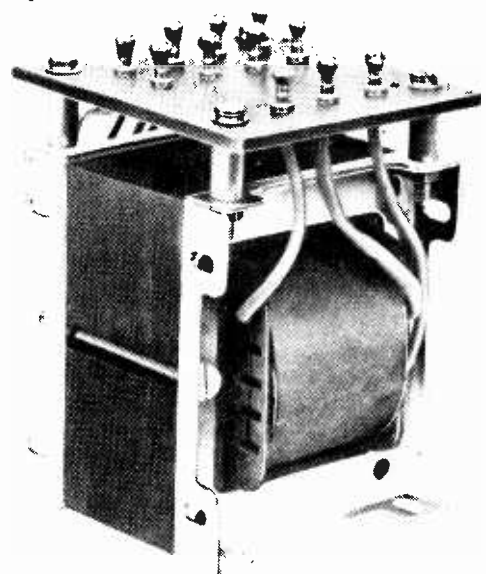
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# Resistance comparator

—with linear fractional off-balance indication

by D. Griffiths Ph.D.

Imperial College, London

## A simple d.c. op-amp design featuring linear reading of percentage unbalance for any arbitrary value of reference resistor without recalibration in the range 100Ω to 10kΩ.

It was not very clear what the design objectives were at the beginning of this effort; they never seem to be in my experience. It appeared that we needed either (a) to display the variation of the reciprocal of the unknown resistance  $R_x$  about some nominal value  $R_f$  with zero output when  $1/R_x = 1/R_f$  or (b) to give a strictly linear output proportional to the fractional deviation of  $R_x$  up to 100% above and below  $R_f$  with zero output when  $R_x = R_f$ . The further proposal that accurately-calibrated percentage deviations should be shown on plugging in any arbitrary value of reference resistor  $R_f$  without recalibration, did not seem to simplify matters.

In the event both requirements (a) and (b) were met in a single circuit design which also gave the proposed constant calibration of the fractional unbalance indication. An accuracy of order 0.1% is achieved with full scale indications of unbalance between 1% and 100% in the range 100Ω to 10kΩ.

The design may be useful on small production runs where resistors have to be hand-trimmed within certain readily-seen percentages of different awkward values; the components used in the original bread-board can then be the master references during trimming. The original application however was with temperature sensors which could be of widely different values although all had

similar temperature coefficients of resistance when expressed as a percentage change; this circuit then gave the same loop gain to a process controller when used with different sensors.

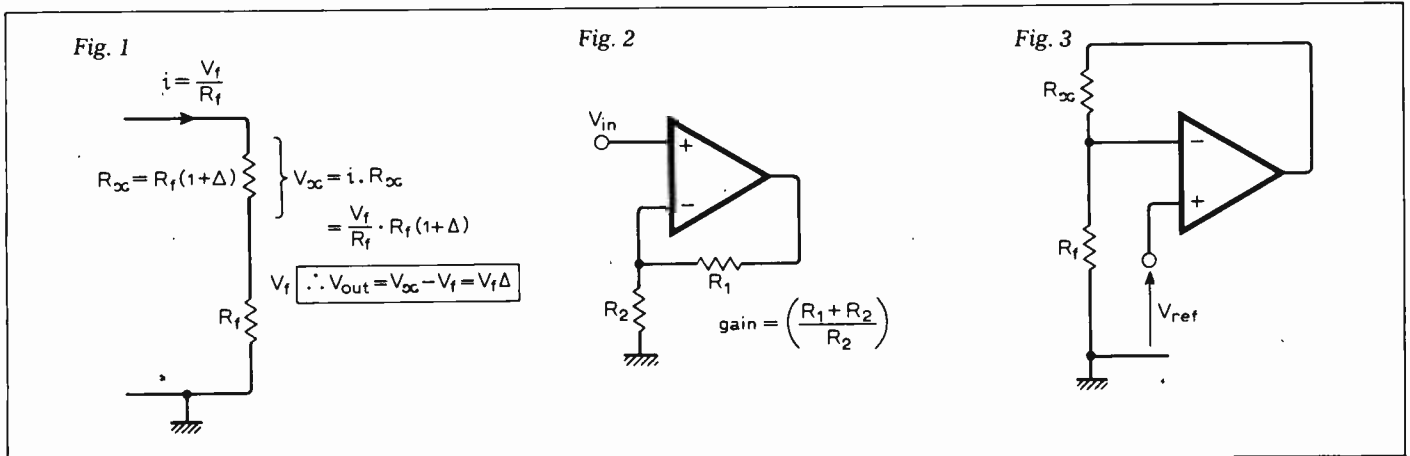
As is often the case it was difficult to get away from the first lines of attack that occur to one at the initial doodling stage; I felt that something in the ratio transformer or Wheatstone bridge line would be required. After all, item (a) involved  $1/R_x$ , i.e. a conductance, and invited a ratio arm transformer technique; but it was not evident how to maintain a calibrated fractional unbalance indication with arbitrary values of  $R_f$  at least with a reasonably simple circuit (watch forthcoming Letters' columns). On the other hand alternative (b), which involved direct display of resistance variations, ruled out a Wheatstone bridge scheme by the wide range of linearity said to be required.

The requirement (b) can be looked at thus: suppose we keep a constant and known voltage across  $R_f$ ; then if the current through  $R_f$  also flows through  $R_x$ , the difference in the voltage drops across  $R_f$  and  $R_x$  will only depend on the fractional relation of  $R_f$  and  $R_x$  and not on their actual values. It then starts to look like an exercise in op-amp techniques, as indicated in Fig. 1. (Requirements (b) can also be met by interchanging  $R_f$  and  $R_x$ .

In the prototype the voltage across  $R_f$  was set at 1 volt, a higher value bringing power dissipation problems in the test resistors. A proposed system accuracy of order 0.1% implied keeping drifts and computing errors to less than 1mV when referred to this 1-volt level. Past experience suggested that a d.c. technique with type 741 op-amps would just suffice to achieve this, especially in view of the comparatively low values of resistance to be compared. (The use of an a.c. carrier scheme would enable  $V_f$  and the power in the test resistors to be set many orders of magnitude smaller but the circuitry would then be a good deal more complex.)

It just remained to convert these ideas into hardware. The functions required are: (1) to hold the voltage  $V_f$  across  $R_f$  constant at 1 volt; (2) to use a differential amplifier to monitor  $V_x$ ; and (3) to subtract  $V_x$  and  $V_f$ , and scale the unbalance appropriately.

Consider first how to hold  $V_f$  constant. In an op-amp follower-with-gain circuit, drawn in the usual way in Fig. 2, the ideal action of the negative feedback is to maintain the inverting input terminal (-) at the same voltage as the non-inverting input (+). This will be so, irrespective of the value of  $R_2$ , provided  $R_1$  is not so large as to cause the output of the amplifier to saturate at either full positive or negative excursion. Calling



$R_1 = R_x$  and  $R_2 = R_f$ , we can redraw Fig. 2 as in Fig. 3, where the voltage across  $R_f$  will be held at  $V_{ref}$ , for an ideal amplifier. This is the first step in a realization of Fig. 1.

The second function to be achieved is that of causing the voltage across  $R_x$  to appear referenced to the common line, so it can be compared subsequently with the voltage appearing across  $R_f$ ; this is the function of a differential amplifier. Such an amplifier can have its input stage operating in the inverting mode, whereupon the common-mode rejection ratio (c.m.r.r.) of the amplifiers does not limit the achievable c.m.r.r. of the circuit. On the other hand, inverting stages usually have a much lower input resistance than follower stages, though in differential applications the latter are limited by the c.m.r.r. of the op-amps used. The choice is easily made here for  $R_f$  has a constant voltage across it which lessens the c.m.r.r. demands on the amplifier and we require a high input resistance to minimize the loading of  $R_x$ ; if  $R_x = 10k\Omega$ , an amplifier input resistance of  $10M\Omega$  will effectively lower this resistance by 0.1%.

Fig. 4(a) shows a high input resistance differential amplifier, while Fig. 4(b) is intended to show how the common-mode rejection occurs by

emphasizing the bridge action through drawing it in a more "Wheatstone" way. If  $R_a = R_b = R_c = R_d$ , and if in Fig. 4(b) both points A and B move up and down in voltage together (i.e.  $V_{AB} = 0$ ), then points C and D will experience equal voltage excursions of one half of this magnitude if E remains at ground potential. This absence of output from the op-amp is consistent with its zero input,  $V_{CD} = 0$  as required.

In Fig. 4(a) the gain to differential input signals is  $-1$  if all the bridge resistors are of equal value. This can perhaps be seen most easily by thinking of the differential input  $V_{AB}$  as riding on top of the common-mode signal  $V_{CM}$  and remembering that ideally  $V_{CM}$  does not affect the voltage at E. Thus one can consider  $V_{CM} = 0$  when thinking only of the differential signal and note that this makes point D at ground potential. Resistances  $R_a$  and  $R_c$  are then evidently seen as a unity-gain see-saw amplifier with phase inversion.

In the prototype circuit the maximum voltage across  $R_f$  had to be limited to 1 volt and to reduce the effects of voltage offset drifts the voltage across  $R_f$  and  $R_x$  was multiplied by three before passing it to the remaining op-amps. The differential amplifier of Fig. 4(a) can give gain by the addition of three resistors as shown in Fig. 5.

If  $R_3 = R_5$ , the voltage gain of the input stage is  $+(1 + 2R_3/R_4)$ . At first glance one might expect the factor of two to be outside the bracket but inspection of Fig. 5 shows that

$$\begin{aligned} V_{AB} &= V_1 + V_2 - V_{IN} \text{ (across } R_4) \\ &= V_{IN} \left( \frac{R_3 + R_4}{R_4} \right) + V_{IN} \left( \frac{R_4 + R_5}{R_4} \right) - V_{IN} \\ &= V_{IN} \left( 1 + \frac{2R_3}{R_4} \right), \text{ if } R_3 = R_5. \end{aligned}$$

Compared with many other difference amplifiers that of Fig. 5 has two outstanding advantages. First, the gain can be adjusted by varying a single resistor,  $R_4$ . Secondly, setting of the gain is quite independent of trimming for best c.m.r.r. It should be noted that if  $R_3$  does not equal  $R_5$  exactly, then this only affects the gain and does not reduce the common mode rejection of the circuit.

The addition of a standard virtual-earth summing amplifier to the circuits of Figs 3 and 5 finishes the design, the complete circuit of which is shown in Fig. 6. A saturated 741 o-amp with  $\pm 15V$  supplies will have an output of 13 to 14 volts and gives only a modest overload to the meter which requires  $\pm 10V$  at the output of  $A_6$  for full-scale deflection. The  $2.2-\mu F$  feedback capacitor reduces needle jitter below the visible limit with a 90-mm scale length meter.

One might imagine at first sight that a 1% change in  $V_{ref}$  (and hence  $V_d$ ) would cause a full-scale change in meter reading when the output stage is on the 1% f.s.d. setting. (If this were so it would place a stringent demand on the stability of  $V_{ref}$  and make the circuit rather unattractive.) This misconception can arise by visualizing a 1% change in the voltage across  $R_f$  and seeing this as giving rise to a 1% unbalance at the input of the summing amplifier. However, this overlooks the changed voltage across  $R_x$ .

It is evident that if  $R_x$  exactly equals  $R_f$  then the output meter will register zero ideally for any value of  $V_{ref}$ . Suppose next that  $R_x = (R_f + \frac{1}{2}\%)$  with  $V_{ref} = 1V$  and the output meter indicates  $+\frac{1}{2}\%$  (i.e. half scale on the 1% range). If now  $V_{ref}$  increases by 1% say, then it is the extra voltage drop across the extra  $\frac{1}{2}\%$  of  $R_x$  (compared with  $\bar{R}_f$ ) that is the unbalanced input to the summing amplifier and will come through to the output; the new output reading would be  $(0.5 \times 101/100)\% = 0.505\%$ . Thus it is the span of the final meter deflection which is affected in direct proportion to possible changes in  $V_{ref}$ .

Fig. 6 shows that  $V_{ref}$  is derived here from the integrated power regulator output; the prototype used MVR15 devices from RS Components. These sort of devices have impressive output stability and modest price. Under constant load and in normal laboratory conditions their voltage drift is not

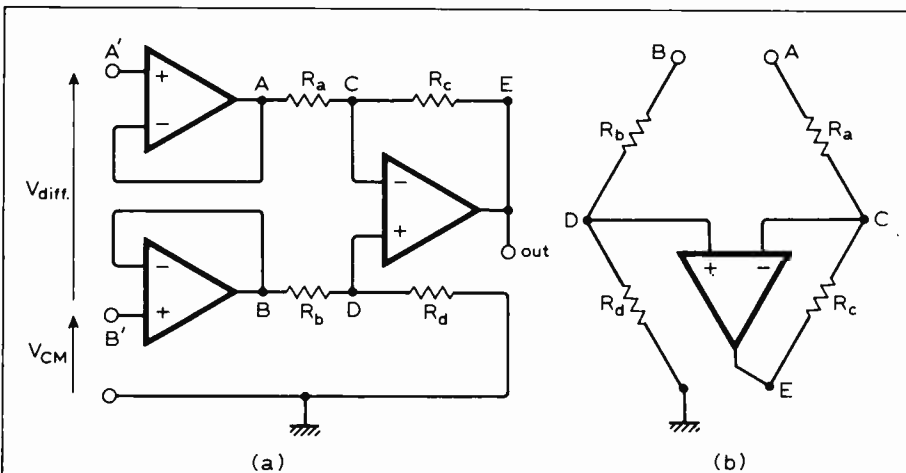


Fig. 4 (a) high input resistance differential amplifier, (b) diagram emphasizing bridge action of (a).

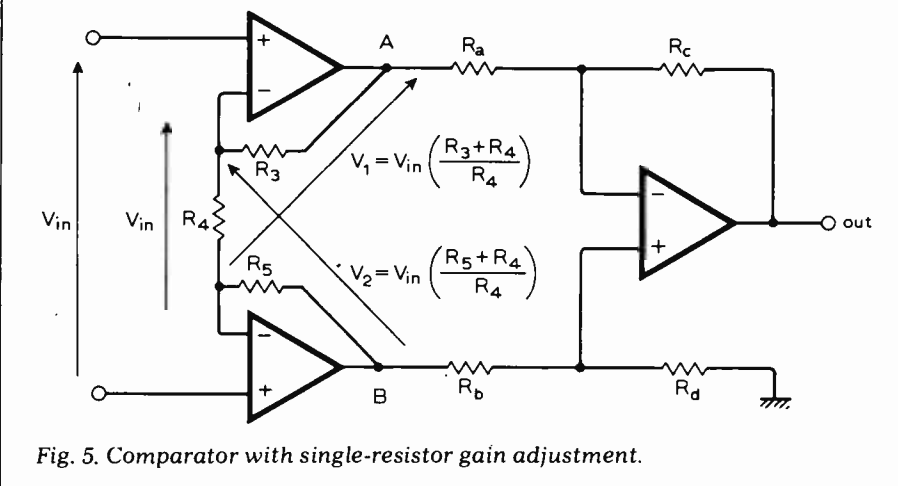
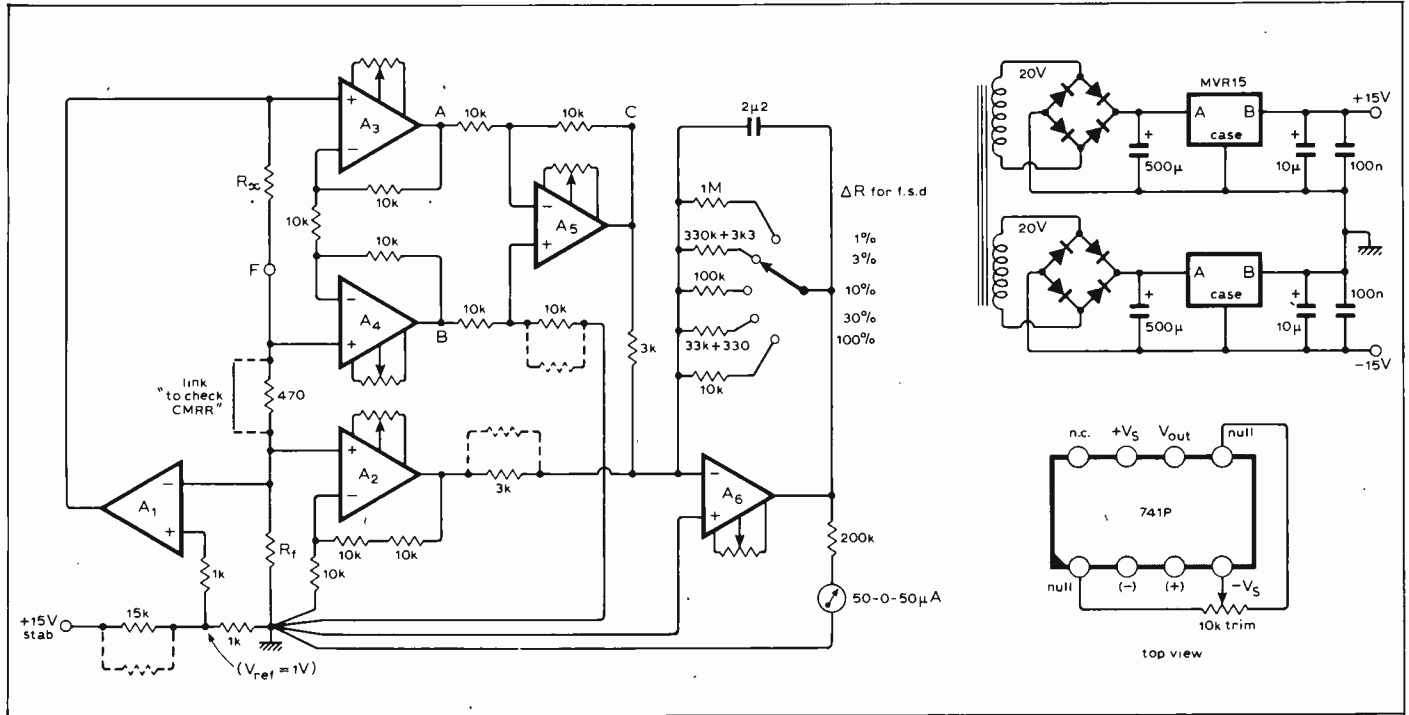


Fig. 5. Comparator with single-resistor gain adjustment.



visible on a 3½-digit multimeter on its 20-V range after a few minutes from switch-on, i.e. the output is steady to better than 10mV. In view of the insensitivity of this comparator circuit to changes in reference voltage, these regulators are more than adequate for supplying the reference voltage here.

Next we describe the procedure to trim the offsets of the op-amps, balance the differential amplifier and equalize the gains to the summing junction. It may sound a shade long-winded but it is quite straightforward and can be done in a few minutes, at least on the second time round.

Type 741 op-amps were used in all stages and the 10-kΩ offset controls were standard miniature carbon presets. The use of cermet-track elements may give a better temperature stability to the balance of the amplifiers but the extra cost is considerable. When trimming these offset voltages it is necessary to short various resistors; constructors are reminded that (a) the resistance of a "short" can sometimes be significant and (b) the short may be carrying more current than was at first thought. A current of only 10mA flowing through 6 inches (pardon, 15cm) of ordinary 2-amp connecting wire (7/0.2mm, 0.22mm<sup>2</sup>) produces a voltage drop of 0.1mV. The zero stability of even ordinary unselected 741 amplifiers is sufficiently good that it is worthwhile zeroing them to at least 0.1mV (referred to the input). As indicated in Fig. 6 a single point earthing scheme is a sensible precaution too. However,  $R_x$  can be quite distant from the rest of the circuit as the potential drop in the input leads to  $A_3$  and  $A_4$  is only that due to the 0.2μA bias currents of the 741 amplifiers.

A 3½-digit multimeter with least significant digit of 0.1mV was used in setting up the prototype; zeroes were adjusted until the + and - polarity

Fig. 6. Complete circuit where  $V_{ref}$  is derived from the integrated power regulator having an output stable within 10mV.

signals were flicking equally. If the 10kΩ preset used with a particular 741 has to be adjusted to more than say 2½kΩ from its mid-track position to balance the offset, it is perhaps prudent to select another 741 in this application.

The trimming procedure is as follows.  
 (1) Short  $R_x$ , trim the offset of  $A_3$  and  $A_4$  to give  $V_{AF} = V_{BF} = 0$ , checking  $V_{AB} = 0$ .  
 (2) Keeping  $R_x$  shorted also short  $R_f$ , measure  $V_{AB}$  (ideally zero) and trim  $A_5$  to give  $V_{CE} = -V_{AB}$ .  
 (3) With  $R_f$  and  $R_x$  still shorted, trim  $A_2$  for zero output, put  $A_6$  to the 10kΩ f.b. setting and trim  $A_6$  to give an output of  $-3.3 \times V_{CE}$  (found in step 2).  
 (4) With  $R_x$  shorted but restoring  $R_f$  to about 500Ω, adjust the balance of the differential 10kΩ bridge until  $V_{CE}$  remains constant when opening and closing the link across 470Ω (marked "to check c.m.r.r.").  
 (5) Select  $R_x$  and  $R_f$  to be exactly the same value (around 2KΩ) and adjust one of the 3kΩ summing resistors to  $A_6$  until the output meter reads zero on the 1% f.s.d. range.  
 (6) See three paragraphs below.

If two resistors of known equality are not available for use in step(5) the comparator can still be used to set up two resistors to the necessary degree of equality. One of the nominally equal pair is made trimmable and adjustment carried out until interchanging these two resistors in the positions  $R_f$  and  $R_x$  causes no change in the output meter reading; it is of no importance if the reading is non-zero at this point since step (5) has not yet been completed.

The prototype on the 1% range had a zero stability of about 0.005% during a normal day and a drift from cold switch-on of about 0.04%.

The linearity of output was checked

on the 100% and 10% ranges with a 3½-digit d.v.m. on the output of  $A_6$  and was found to be better than 0.1% ( $\pm 1$  digit) with  $R_f$  of 200Ω, 1kΩ and 5kΩ and full-scale unbalance on either side of equality. This good linearity makes scaling of the output ranges easy and the final item of the trimming procedure, step (6) is: With  $R_x = 0$  and the output stage on the 100% range, then for any value of  $R_f$  (100Ω to 10kΩ) the meter is made to read -100% by trimming the voltage divider giving the nominal 1 volt reference. Accuracy of the scale of the remaining ranges depends almost entirely on the accuracy of the f.h. resistors around  $A_6$  since the open-loop gain of a 741 at zero frequency is typically about  $10^5$ .

And what, you may ask is the fudge which is ill-concealed by the 1-kΩ resistor forlornly stuck between the + terminal of  $A_1$  and the point marked  $V_{ref}$  in Fig. 6? Well, it is tied up with the 100-Ω and 10-kΩ limits which were so casually mentioned earlier without explanation. The lower limit is set by  $A_1$  running out of the enthusiasm for supplying current much greater than 10mA, at least to the 0.1% accuracy required here. The prototype was satisfactory of  $R_f$  down to 70Ω and lower values could doubtless be accommodated by buffering the output of  $A_1$  with a power transistor. The upper limit arises from errors due to the bias currents in the increasing source resistance presented by  $A_1$  by  $R_f$  and  $R_x$  in parallel. Making the source resistance of  $V_{ref}$  about 2kΩ (as seen by  $A_1$ ) distributes this offset equally for  $R_f = 100Ω$  and 10kΩ: on the prototype this error amounted to  $\pm 0.07%$ , causing high values of  $R_x$  to read low by this amount. Substituting superbeta or f.e.t.-input op-amps for the 741 would enable the upper resistance limit to be pushed up.

# Realm of microwaves

## 10—Power and frequency measurements

by M. W. Hosking, M.Sc.

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At the low frequencies, where a cyclical change of current and voltage can be recorded and where the wavelengths are many orders of magnitude greater than the transverse dimensions of a conductor or component, it is possible to insert a current- or voltage-measuring instrument into the circuit to determine these quantities. The instrument itself has either a negligible or precisely known (internal resistance) effect on the circuit and one knows, say in the case of an ammeter, that it is indicating the total current flowing at that point.

Consider, however, the case of a hollow, metal waveguide: to d.c. this is a single conductor and one has difficulty with the concept of a "potential difference". Furthermore, as shown earlier in this series, the microwave current flows in circulating loops confined closely to the metal surfaces, and even were it possible to measure this current directly one could not say that this was the total current associated with an overall potential. It thus becomes conceptually inconvenient to think in terms of current and voltage as well as impracti-

cal to measure, and so these more fundamental quantities are lumped together and it is the total, time-average power which is measured.

Compared with the accuracy to which d.c. or low-frequency power can be measured, the absolute determination of microwave power is rather poor. Typical day-to-day accuracies using standard commercial power meters lie between 5% and 10% and even national standards are only in the region of 0.5% accurate. The fact that high-quality tracking and communication systems have evolved in spite of this limitation demonstrates that it is only on comparatively rare occasions that a highly accurate knowledge of power is necessary. Even then, it is usually required during the development of other

instruments. In the majority of cases the important factor is the power difference between one space or time and that in another space or time, i.e. relative power. Using standard laboratory test gear relative microwave power can be measured to within a small fraction of 1%.

As yet there is no practical, absolute method of microwave power measurement; that is, one which will indicate microwave power directly without calibration or transfer from some more primary effect. Although varied principles and techniques have been proposed and demonstrated over the years, the most practical way of determining microwave power has been by using some element to absorb the power and then observing the resulting heat dissipation. Devices used can conveniently be placed in one of two categories:

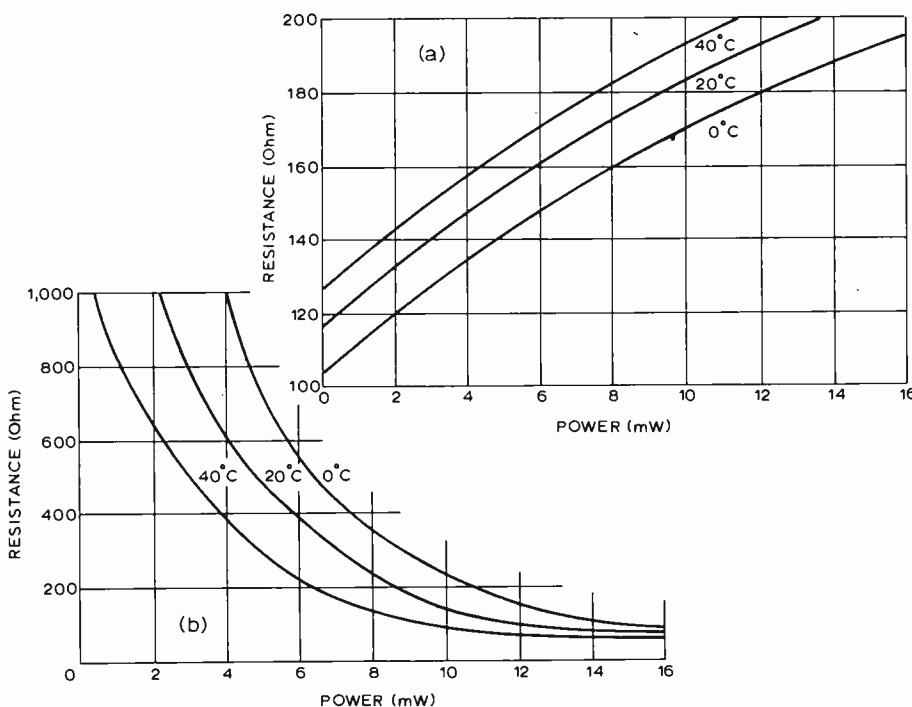
- in which the dissipated power produces a change in the electrical resistance of the absorbing element (called a bolometer), or a voltage difference (called a thermocouple);
- in which the rise in temperature of the dissipating element is measured and calibrated to read power (called a calorimeter).

These two groups are by no means exhaustive and there exist both variations and completely different methods of indicating microwave power. However, this series is essentially concerned with the real world of microwave electronics and, in this context, the above categories are the only ones of practical use.

### Bolometric devices

Bolometers are temperature-sensitive resistances taking the form of either a thin resistive wire or film, called barreters, or small-bead thermistors. Calibration of these elements is carried out by low-frequency substitution; that is, the change in resistance with microwave power is noted and identified with the d.c. power necessary to produce the same change. Here one starts off with the chain of accumulating errors in the microwave power-measuring system by asking: does the

*Fig. 1. Most common bolometric elements consist of either a very thin platinum wire having response curves shown in 1(a) or else a thermistor bead having the opposite type of response shown in 1(b).*



d.c. power represent the total incident microwave power? The answer is that it need not do so and several requirements have to be met before the answer can be changed to "yes" with confidence.

These requirements are that the cross-sectional dimensions of the wire or thermistor should be similar to the skin depth at the operating frequency, so that the d.c. and a.c. densities are similar; and that the physical length of the device should be as small as possible to minimize the very significant inductive reactance.

As a consequence, the barreter is usually constructed from a length of silver-plated platinum wire having a section perhaps 1mm long of the silver etched away, exposing the resistive platinum wire to the microwave field. This wire is very thin, typically 0.002mm in diameter, and is mounted inside a sealed cartridge or on a dielectric support of suitable dimensions for mounting in a waveguide or coaxial monitor. Barreters have a positive temperature coefficient of resistance, and a resistance/power sensitivity shown in Fig. 1(a). They have a very short thermal time constant of several hundred microseconds, useful for fluctuating signals, but this can produce errors when measuring the average power of a pulsed waveform because of the tendency to respond to the signal peaks.

Most popular of the general run of power-sensing elements is the bead thermistor. Composed of semiconducting, sintered metallic oxides, the bead is about 1/4mm diameter with two very fine wire contacts and has a negative coefficient of resistance. Its resistance/power sensitivity, shown in Fig. 1(b), is much greater than that of the barreter, operating temperature can be higher, it is more rugged and has a thermal time constant several times longer.

Whichever type of bolometer is used, most power-measuring instruments come in two units. One is the bolometer mount, consisting of the microwave input connection, either waveguide or coaxial, in which the wire or thermistor forms an absorptive termination, plus a relatively large thermal mass. The second is the meter with associated circuitry, connected to the mount by flexible cable carrying d.c. or low-frequency bias signals.

Within the meter the basic circuit is the balanced bridge with automatic feedback shown in Fig. 2 in which the bolometer element forms one arm. A suitable resistance, usually 100 to 200 ohms, is selected for the element to balance the bridge and is achieved by passing low-frequency current through the element. Audio frequency power is usually chosen for ease of measurement and amplification and, in the case of the thermistor, Fig. 1(b) shows that the current required for a single bead lies between 1 and 15mA.

At this stage, with no microwave power present, the bridge is balanced

and the meter reading will be zero. With microwave power present, however, the thermistor will be hotter, its resistance will decrease and, in order to maintain a balance, the audio power must decrease by an amount equal to the microwave power, which can then be identified and displayed. There are many refinements adopted to preserve accuracy and stability in commercial instruments, but the balanced bridge remains the heart of the circuit. The dynamic range of these instruments is generally 40dB with good sensitivity, switchable meter ranges lying between 10 microwatts full scale and 10 milliwatts full scale.

Within the bolometer mount itself lie the sensing elements, usually thermistors, a large thermal mass to help reduce fluctuating external temperatures and also a couple of other thermistors to sense changes in ambient temperature. These latter are not connected to the microwave circuit but form part of another bridge within the power meter and help to distinguish between

ambient temperature variations and changes in microwave power. With a large thermal mass, this may appear trivial but, when measuring a few microwatts of power, a 25% meter drift can easily occur with an uncompensated mount.

To be accurate the sensing elements in the microwave circuit must, ideally, form a perfectly matched termination to the transmission line. In the case of standard 50-ohm coaxial line, Fig. 3 shows a mount and method of thermistor attachment. Two beads are used and are mounted between the inner and outer conductors to give the type of electrical circuit shown in Fig. 4.  $C_1$  is a d.c. blocking capacitor to eliminate spurious effects from the source and of the circuit and, with a value of 1 to 2nF, has a very low reactance at the microwave input frequency.

For convenience in biasing and matching, two thermistors are used and are connected in series as far as the audio frequency substitution circuit is

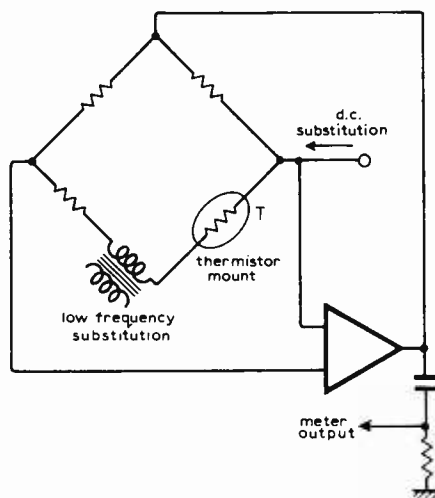
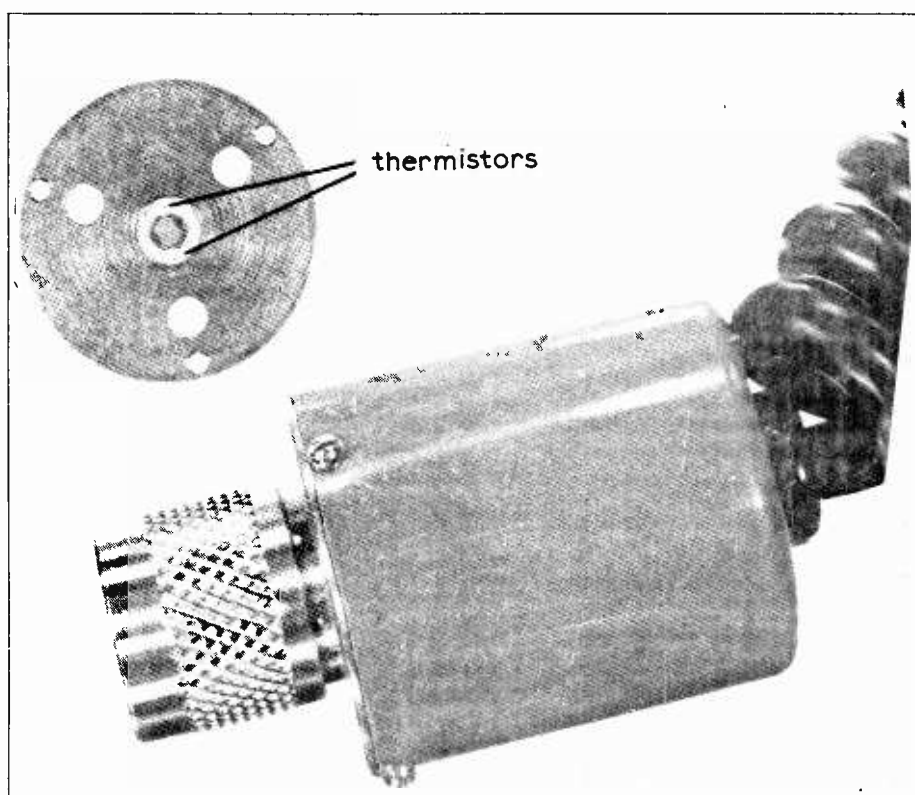


Fig. 2. Variations in bolometer resistance due to incident microwave power are detected by a resistive bridge. The substituted d.c. power to rebalance the bridge is an indication of the microwave power level.

Fig. 3. Coaxial thermistor head in which the thermistor beads terminate the transmission line in a good match and so absorb the microwave power. Head is electrically connected to the power meter bridge, amplifier and display unit.





concerned. They are biased to a value of 100 ohms each. Capacitor  $C_2$  is similar in value to  $C_1$  and thus also presents a low impedance to the input signal, the effect being to cause the thermistors to appear in parallel at r.f. Overall impedance presented to the 50-ohm transmission line is thus 50 ohms and helps towards achieving a good match. The compensating thermistors are electrically isolated from the microwave circuit but are in close enough thermal proximity to experience, identically with the detection thermistors, any variation in ambient temperature.

With a range of waveguide mounts also available, the thermistor power meter is a sufficiently accurate and reliable instrument and, for many years, has been the backbone of engineering power measurements.

### Thermocouple power meter

A strong challenge to the position of the thermistor is being made by the thin-film thermocouple and, with the improvements made in recent years, this device now offers several advantages such as very much greater temperature stability and higher burn-out levels. The coaxial mount construction is very similar to that of the thermistor except that, instead of fine wire supports, the favoured technology is that of thin film deposition on as thin as possible a substrate.

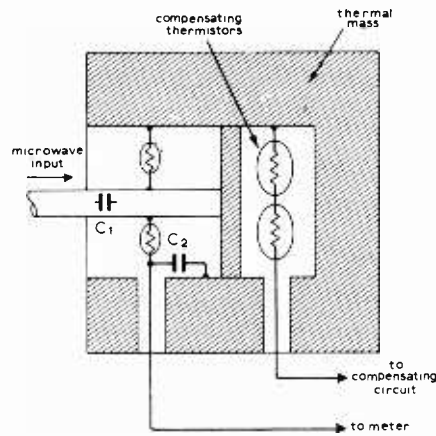


Fig. 4. Thermistors which terminate coaxial line appear in series to the d.c. substitution and bridge circuit but in parallel to the high-frequency microwaves. A large thermal mass together with twin compensating thermistors substantially eliminate ambient temperature fluctuations.

An example is shown in Fig. 5, the thermocouple being formed from evaporated bismuth and antimony with the hot junction lying in the gap between centre and outer conductors; the large semicircular contact pads are of gold.

Thermocouple resistance, and hence match, are controlled by the bismuth and antimony film thickness. Incident

microwave power absorbed at these hot junctions raises their temperature, giving rise to a thermoelectric voltage which is then amplified and displayed in terms of microwave power.

The voltage generated in this fashion can be as low as several hundred nanovolts and thus requires careful circuit design to avoid odd thermocouple effects creeping in from dissimilar metal junctions and other sources of noise. Amplification is carried out after first chopping the d.c. signal and the signal is then synchronously detected. Unlike the bolometric power element, instrument calibration is carried out by direct comparison with a national substandard and not by d.c. substitution.

Recently an improved form of thermocouple sensor has appeared on the market\* using a silicon p-n diffused region as one arm of the thermocouple with a gold contact to act as the cold junction and a resistive tantalum nitride contact as the hot junction. The complete element is less than 1mm square and 0.005mm thick and offers a better r.f. match because of lower reactance, a faster response time and greater long-term stability than the normal bismuth-antimony element.

### Calorimeters

In contrast to the devices so far mentioned, in which microwave power is measured by some calibrated change in an electrical property, the calorimeter relies upon dissipating the incident power within some absorbing medium and then measuring the associated rise in temperature. The microwave power can then either be calculated from a knowledge of the temperature rise versus time and the thermal mass, or a calibration can be made against known quantities of d.c. or low-frequency input power.

Commercially available calorimeters are bulky and expensive devices and have measurement rise times of several minutes. Consequently they are usually kept in the standards room of the user as a calibration reference for the more general-purpose bolometric instruments. Higher-order standards tend to be individually designed and vary from country to country and are always being improved. Thus, although the operating principles are the same, there are many different types of calorimeter. Instead of enumerating these, it will probably be of greater interest to describe briefly one of the instruments which has recently been developed at the National Physical Laboratory for use as a national standard.

### NPL calorimeter

This device is a twin calorimeter and operates in the system shown in Fig. 6 between d.c. and 6,000MHz and for input power levels of between 10mW

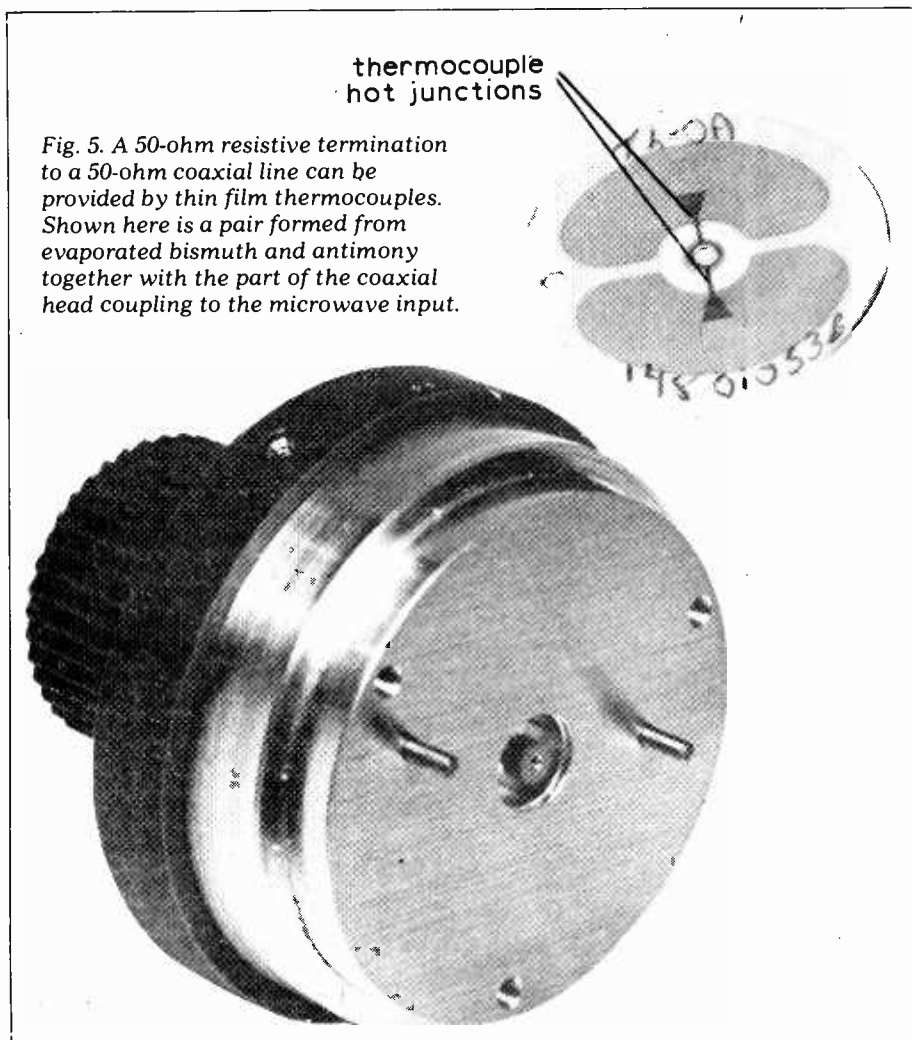


Fig. 5. A 50-ohm resistive termination to a 50-ohm coaxial line can be provided by thin film thermocouples. Shown here is a pair formed from evaporated bismuth and antimony together with the part of the coaxial head coupling to the microwave input.

\* Hewlett Packard Journal, Sept. 1974.

and 100mW. The instrument uses two coaxial transmission lines of 50-ohm characteristic impedance, each terminated in a matched, power-absorbing, resistive load. Microwave power is fed into one of the lines and the resulting rise in temperature difference between the two matched loads is measured by the thermopile. This unit consists of 800 junction pairs of copper-constantan. The loads and thermopile at the end of the calorimeter are shown in Fig. 7. After the heating effect is noted the microwave power level can be determined by measuring the amount of d.c. power which must be applied to the load to produce the same effect. The symmetry of the calorimeter, together with the double-packed thermal insulation, helps to eliminate the effects of room-temperature fluctuations.

An interesting technique used in the development of this NPL calorimeter and in building up a thermal equivalent circuit was the determination of thermal resistances by localized heating with a laser beam. Instead of supplying heat to the calorimeter and noting the temperature response in different areas with thermocouples, these areas were painted black and irradiated with a laser beam, so producing an output from the thermopile. By calculating the local thermal capacities from a knowledge of dimensions and using the laser technique to measure the local resistances, a very comprehensive equivalent was obtained.

In practice, to speed up the reading time the calorimeter is operated in a feedback loop wherein the output from the thermopile is fed via an amplifier and frequency-compensating network back to the second input of the calorimeter. The load at the end of this line is thus heated to the same temperature as that terminating the microwave input and the microwave power can be determined from the substituted d.c. input power necessary to produce the same power in the feedback loop.

With corrections made for losses in the input lines, power lost in heating the thermopile, load mismatch error and d.c. instrumentation errors, the absolute accuracy in measuring the microwave power lies between 0.2% and 0.5% with a measurement time of several minutes.

So, even for a national standard, the accuracy with which microwave power can be measured is not as good as that for d.c. or low-frequency power. The uncertainty of the d.c. calibration power in the calorimeter, for instance, was an order of magnitude loss. Even so the general purpose commercial instruments are many times worse than this in absolute accuracy and it is worthwhile noting the prime causes of error.

#### Power measurement errors

There are three main sources of error:

- instrumentation error,
- d.c. substitution error,
- mismatch error.

The first is not particular to microwave measurements as it is caused by such things as amplifier non-linearities, range switching and meter display, but might typically lie in the region of 1% of f.s.d. The substitution error has been mentioned previously and is due to the d.c. or low frequency power producing a slightly different heating effect than the microwave power. As such it is a function of the sensing element dimensions compared with the wavelength and is different for the barretter, thermistor and thermo-couple. Usually the error is quoted as an efficiency defined by

$$\frac{\text{d.c. substituted power}}{\text{dissipated microwave power}}$$

and can be quite significant, typically lying between 90% and 99% depending upon frequency. The way round this error is by the instrument manufacturer maintaining a standard microwave power reference source and calibrating each sensing element. An efficiency versus frequency plot is then supplied with each mount and a manual control allows for compensation. By this means the substitution error can be made smaller than the other two main sources.

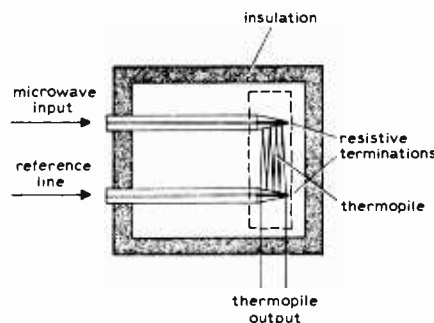
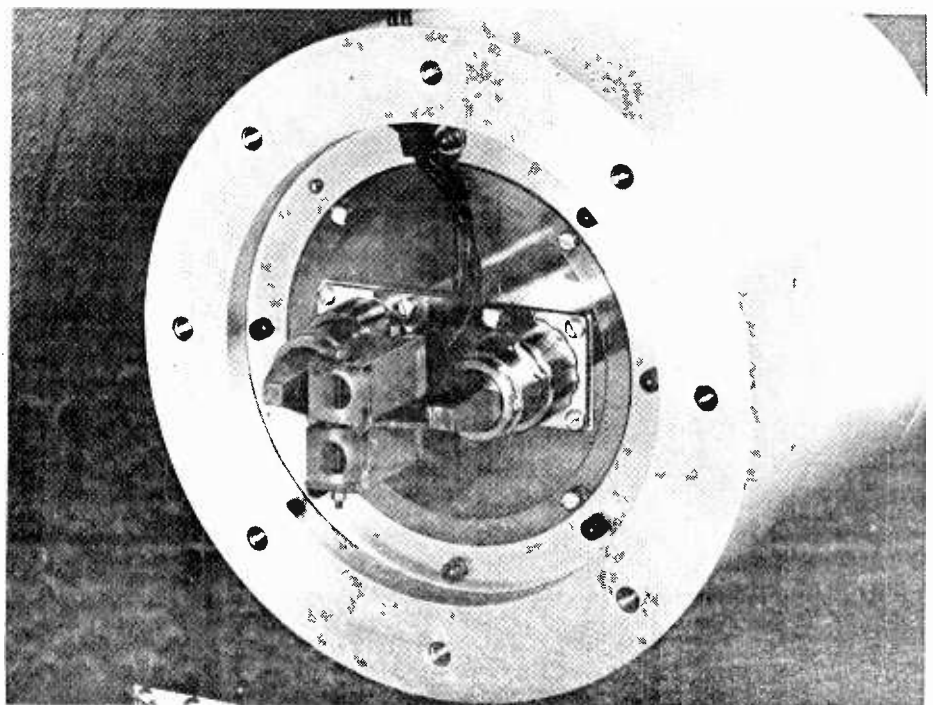


Fig. 6. Schematic of a twin calorimeter wherein the microwave power is absorbed in a resistive load and the resultant rise in temperature measured and calibrated.

Fig. 7. Rear view of the NPL calorimeter showing the resistive load terminations and thermopile coupling. (Courtesy National Physical Laboratory, Crown Copyright reserved.)



duced, the day-to-day practice is for manufacturers to design components to as low a v.s.w.r. as possible and for the user to accept the resultant error.

By way of illustration and to recap on previous subject matter: the ratio of the electric field magnitude reflected from a mismatch to that incident is termed the voltage reflection coefficient ( $\rho$ ) and this reflected signal gives rise to a transmission-line standing wave pattern as shown in Fig. 1 of Part 9. The ratio of the electric field maximum to minimum of this pattern, which can be directly measured, is termed the voltage standing wave ratio  $S$  (v.s.w.r.), and is universally used as an indication of the degree of mismatch of a component. A perfect match is when  $S = 1 + \rho / 1 - \rho$  remembering that, in general,  $\rho$  is the modulus of a more complete reflection coefficient containing phase information.

Now when two or more sources of mismatch are present the amount of power that is actually reflected from any one of them depends upon the way in which the reflected waves combine, that is, upon their relative phase, and this is the quantity usually unknown. It is, however, possible to define a worst case and a best case limit to the resultant mismatch from just a knowledge of the v.s.w.r.s involved. Take the case of a microwave generator having v.s.w.r.  $S_1$  and power monitor of v.s.w.r.  $S_2$  ( $S_2 > S_1$ ), then the worst combination would be if one had a v.s.w.r. of  $S_1$ ,  $S_2$  and the other unity, and the best case would be if one were  $S_2/S_1$  and the other unity.

Taking some practical values of  $S_1 = 1.30$  and  $S_2 = 1.50$ , which are typical for general test equipment up to J-band (12.4GHz), the worst and best cases result in values of 1.95 and 1.15 corre-

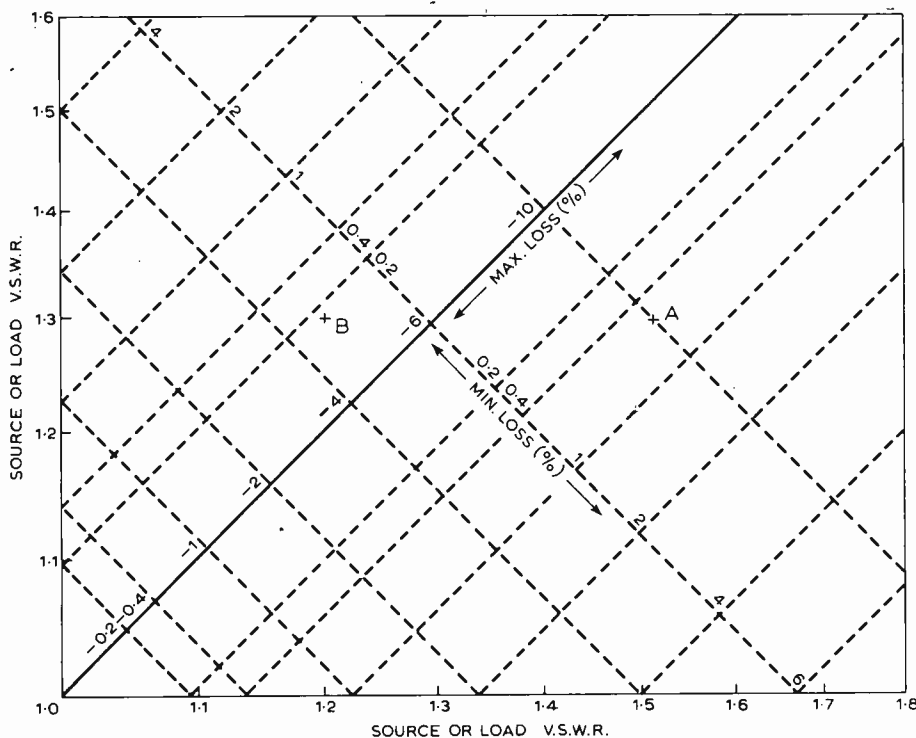
sponding to values of  $\rho$  of 0.32 and 0.07 respectively. The power reflected is proportional to  $\rho^2$  and so, in this case, the power meter error will lie between -10.2% and -0.5% depending upon the way in which the mismatches combine. A reduction of the power monitor v.s.w.r. to, say, 1.2 would have a significant effect on the error, reducing the uncertainty range to between -4.8% and 0.2%. The way in which other variations in match can effect the power measurement error is shown in Fig. 8 in which the above two cases are plotted as points A and B. It can readily be seen how easy it is to introduce quite large errors into microwave power measurement and how important it is to minimize the mismatch loss of microwave components.

A final point concerning Fig. 8: the percentage error introduced by combining the v.s.w.r.s on this basis is that compared to what would be delivered to a power monitor having an impedance equal to that of the transmission line.

**Measurement of frequency**

In general the direct measurement of frequency is basically a measurement of time but, because of the manageable size of wavelengths in this region of the spectrum, frequency can also be determined by a measurement of length. An example of this latter method is the slotted line used for v.s.w.r. measurements previously dis-

*Fig. 8. Effect of the mismatched source and load can be quite serious in terms of measurement error. This graph shows the limits of maximum and minimum loss set by two mismatches; the exact value cannot be determined without phase information, which is usually lacking.*



cussed in Part 9. By moving the sliding carriage, the attached probe samples the periodic standing wave pattern in the transmission line which repeats itself every half wavelength. The position of the carriage is indicated by a calibrated vernier scale like that used in vernier calipers or sometimes by a clock gauge. In either case position can be measured to about 0.1%, but this accuracy is somewhat degraded when applied to measuring wavelength because of the error in finding the identical probe positions on different cycles of the pattern. This method is comparatively laborious and is only used nowadays either as a teaching aid or in those cases of dire emergency when one's own frequency counting system has broken down and one can't borrow a replacement from someone else.

A second frequency-measuring instrument, and the most widely used of all, is the wavemeter. Many designs exist but all are based on noting the response of a three-dimensional microwave cavity at its point of resonance, this point being adjustable. A popular method is shown in Fig. 9, which illustrates a cylindrical cavity into which slides an adjustable spindle. The cavity is loosely coupled to the main transmission line so that a small amount of microwave power can enter.

With the spindle withdrawn completely from the cavity a waveguide mode can exist, and the cavity will appear as an electrically resonant circuit with a resonant frequency determined by its diameter. As the spindle is inserted the resonant frequency is reduced from this upper limit and becomes a function of the spindle length,  $L$ , and the cavity now supports a hybrid mode consisting of the original waveguide one and a TEM mode due to the coaxial section formed by the spindle.

Finally, as the spindle penetration becomes greater, the fringing capacitance between the end of the spindle and the base of the cavity starts to influence the resonant frequency, which starts to decrease quite rapidly. The Q factor of this type of microwave resonant circuit is a function of the ratio of cavity to spindle diameters and can be in the vicinity of 1,000.

A practical realization of the instrument is shown in Fig. 10, in this case for use with miniature coaxial connectors. The right-hand component is inserted in series with the coaxial line carrying the frequency to be measured so that the microwave power enters the left-hand connector, say, and leaves via the right-hand one, which might be terminated in either a crystal detector or a power meter. The hole by which a sample of the power can be coupled out can be clearly seen between the two connectors.

On the left of Fig. 10 is the other part of the wavemeter, which contains the cavity, spindle and frequency readout

Fig. 9. Popular version of the wavemeter cavity in which the resonant frequency is governed by the spindle penetration. Cavity is coupled electrically to the main transmission line and the frequency is indicated by the point at which the cavity absorbs power at resonance.

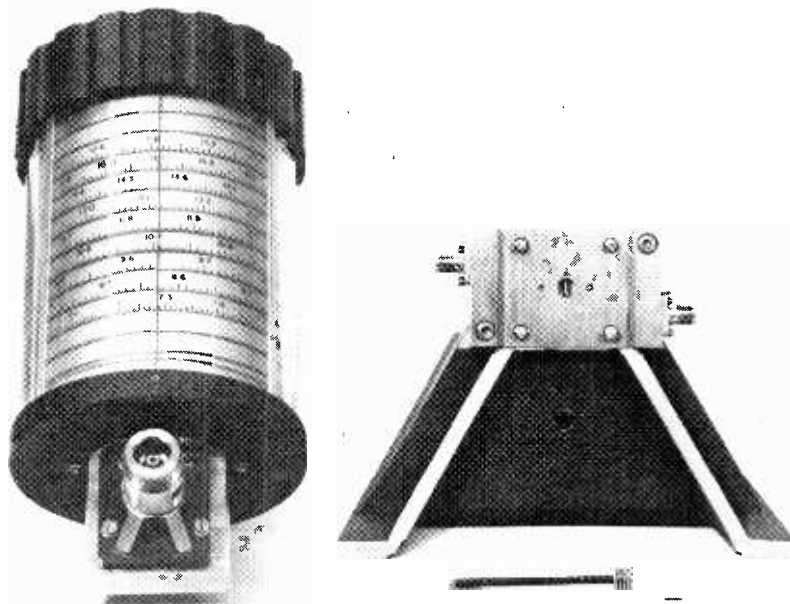
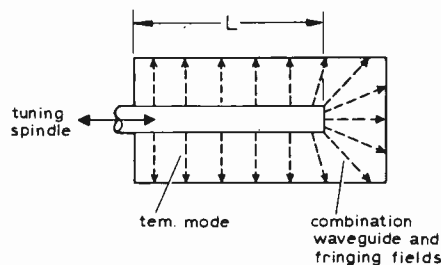


Fig. 10. Commercial wavemeter operating from about 5 to 18GHz, showing the series-mounted section and coupling hole on the right. Bolt-on unit on the left comprises the tunable cavity and frequency readout.

and which bolts onto the other component. Thus, when measuring an unknown frequency, the large drum carrying the scale is slowly rotated, thereby turning also a micrometer thread carrying the spindle and varying its penetration into the cavity. When the point is reached where the cavity is resonant at the transmission line frequency, it will absorb energy from the main line and a sharp dip in output will be observed from the detector or power meter.

The instrument is calibrated from a frequency standard and the advantage of this type of readout is that it enables a large, finely graduated scale to be used. In this case the unwound scale length is about 2m and the measurement accuracy is  $\pm 0.1\%$ . The larger type N connector in the photograph is an additional facility and enables the resonant condition to be identified by connecting a detector to monitor the power absorbed into the cavity.

Progressing in complexity (and cost), one comes to the frequency counter type of instrument which is a true

frequency meter in that it actually counts the cycles of a periodically varying waveform. For microwave frequencies the counter usually consists of two sections: a low-frequency part containing a crystal-controlled reference oscillator, digital counter and digital display and a high-frequency section containing a transfer oscillator, harmonic selector and r.f. input.

The transfer oscillator consists of a conventional low-frequency oscillator circuit operating at, say, 100MHz and it could either be a highly stabilized one or tunable by several tens of MHz either side of the fundamental, depending upon the approach adopted by the manufacturer. Whichever it is, the output from the oscillator is fed to an harmonic generation circuit producing usable outputs up to, say, the 100th harmonic.

Taking the tunable version as an example, the oscillator output plus harmonics would be fed to a tunable mixer along with the input signal to be measured. Harmonic selection circuitry then allows the harmonic nearest to the unknown frequency to be selected, to producing a low i.f. from the mixer which is displayed on an integral c.r.t. The fundamental oscillator can then be tuned to a frequency which gives a zero beat between the two mixer inputs, at which point the unknown frequency is now a known number of harmonics up

on the fundamental and is displayed on a digital readout. In arriving at this correct display it is necessary to know the fundamental oscillator frequency and this is counted directly by shift register in the low-frequency section. Here a reference oscillator accurately times the opening of a sample gate while the number of cycles passing is counted.

Accuracy of these counters is  $\pm$  one count in the low-frequency section, in this case at a nominal 100MHz plus crystal stability. This latter is typically 1 in  $10^7$  per week or 2 in  $10^{-9}$  per second with high stability options giving 1 in  $10^9$  per day. Most instruments also possess a switchable a.f.c. loop which eliminates zero beat error in this case and also enables f.m. signals to be counted.

At present, commercial instruments are available with transfer oscillator plug-ins which enable frequencies of up to 40,000-MHz to be directly measured. But, in principle, the technique can be applied to higher frequencies still.

**Acknowledgment** Many thanks to my old friends at the Sanders Division of Marconi Instruments Ltd for the photographs used in Figs. 3, 5 and 10 and also to Dr Alan Fanton at the NPL for details of the 6GHz calorimeter.

## Sixty Years Ago

ONE of the earliest methods of viewing response curves, now the province of cathode-ray and pen recorder instruments, was described in the issue of *Wireless World* for July 1915. Designed by Dr. J. A. Fleming (Sir Ambrose, of diode fame) the instrument was named the "Campograph" and was reminiscent of the Duddell oscillograph, in that it was "all done by mirrors".

A long, narrow mirror, mounted with its long axis horizontal, was connected by a cord to the spindle of a rotary potentiometer (a new device invented for this instrument) and was tilted as the pot. was turned. The wiper of the pot. derived a voltage which was applied to the device under examination (detector, valve, etc.). A mirror galvanometer, whose light spot was directed on the long mirror, was deflected by the dependent variable signal, such as anode current, the two together forming X and Y axes of the display, projected either onto a screen or photographic plate. Alternatively, the pot. could be replaced by a variable capacitor, when the instrument could be used to plot resonance curves.

Examples of photographs obtained in this way were shown in the article and included valve characteristics, hysteresis curves of iron wire and resonance curves. An instrument which uses a similar principle was described by H. J. N. Riddle in the issue for November, 1971.

# World of Amateur Radio

## Amateurs and emergencies

From time to time amateur radio finds itself firmly at the centre of the world stage — unfortunately most often in connection with major natural disasters that disrupt normal telecommunications leaving amateur stations as the only or first links with the stricken areas. Magazines from Australia and New Zealand reflect two such events: one last Christmas, the other in 1931.

*Electronics Australia* describes how when the cyclone struck Darwin on Christmas Day one of the first links to be established was from a mobile station in a car 13km outside Darwin operated by VK2BNN, his wife VK2BYL and VK8JT. They made contact with amateurs in Victoria more than 1,600 miles away, providing one of the few channels for police and emergency traffic. On Boxing Day an emergency s.s.b. net was established on 14.111 MHz with VK3AUP, Melbourne acting as control. VK8CW at Alice Springs acted as a relay station when required. By December 27 the net had become a nationwide system with participating amateurs in Cairns, Townsville, Rockhampton, Mackay, Mt Isa, Brisbane, Lismore, Armidal, Sydney, Canberra, Cooma, Melbourne, Adelaide, Perth and Alice Springs.

The New Zealand journal *Break-in* reports the death of James Mills, ZL2BE of Hastings who for many years was a leading figure of amateur radio in that country and whose activities attracted world interest in February 1931 when a major earthquake shattered the towns of Napier and Hastings. James Mills was one of the few amateurs having a rotary generator that could be run from car batteries and was able to make contact on 3.5 MHz, first with other amateur stations and then with the official New Zealand Government station ZLW at Wellington, handling a very large number of emergency messages. Later a relief expedition to Napier was accompanied by ZL2BO who set up a station there. The events generated enormous goodwill towards amateur radio and the country still maintains an Amateur,

Radio Emergency Corps which is frequently called upon to help; two recently reported cases involved a search for lost hikers who got into difficulties crossing the Roaring Meg River and a coastal rescue when a trawler went ashore off New Plymouth.

In the United Kingdom the "Raynet" or Radio Amateurs' Emergency Network of the RSGB maintains preparedness for emergency operations through local controllers and groups and by regular exercises in conjunction with the British Red Cross Society, the St John Ambulance Brigade and the police. They are ready and authorised to provide communications assistance on request from the user organisations in conditions where there is a real risk to human life, in the belief that Raynet is a way in which radio amateurs can use their knowledge as a service to the community. Fortunately, the occasions on which Raynet is called upon in earnest are relatively few: most "on air" activity is during simulated emergencies. Nevertheless it is a service that believes in being ready and willing.

## Hourly propagation forecasts from WWV

For amateurs and short-wave listeners a source of hourly propagation data is the American standard frequency transmissions from WWV (Colorado) and WWVH (Hawaii) on 2.5, 5, 10, 15, 20 and 25 MHz. These now include at 14 minutes past each hour an indication of solar flux (in the form 72 plus 0.6R) and geomagnetic activity (0 to 9 K scale).

In general for good h.f. conditions the higher the solar flux figure the better (for the next few years this is unlikely very often to exceed 100); conversely a low K figure (preferably 2 or under) is a good sign. High K ratings indicate a significant influx of solar particles, usually resulting in weaker signals, increased fading and noise: over 4 usually indicates a solar storm; 3-4 unstable or unsettled conditions. Unfortunately at the present time the standard frequency transmissions heard most strongly in the UK are seldom those from WWV or WWVH.

There is growing evidence to suggest we are now very close to the end of the present sunspot cycle, with its oddly distorted decay during 1972. Although it is unwise to make long term predictions about future sun-spot activity it looks increasingly as though the next cycle may have a relatively low maximum.

The ZB2VHF beacon station at Gibraltar is now in operation on 144.145 MHz beaming signals towards the UK.

## Look no batteries!

The energy crisis has made numbers of amateurs look quite seriously into the question of how radio communication could be maintained completely independently of mains supplies or primary batteries. Some recent experiments

have been based on solar batteries, wind generators and pedal- and hand-operated battery chargers. QST for example reports that a man on a jacked-up bicycle can generate 100 to 120 watts of power by driving a car generator at over 1,100 r.p.m. using the high gearing provided by a 27-inch wheel (generators for this purpose were dropped by the RAF to the French resistance during World War II).

But for sheer ingenuity a prize must surely go to a Dutch amateur J. M. H. Wagenmans, PA0HWE who claims to have built a milliwatt transmitter powered entirely by the action of the Morse key! He does this by linking the moving arm of a Morse key to the cone of a moving-coil loudspeaker so that the movement produces an electrical output which is rectified and stored in a 40,000 $\mu$ F capacitor to power a transistor crystal oscillator to a d.c. input of 1.5 mW. Brass pounding with a vengeance; although a nagging doubt remains, despite the photographs and circuit details in the April issue of the Dutch journal *Electron*: April issues of amateur journals are notorious for elaborate technical spoofs, though it is difficult to fault this idea!

## In brief

The RSGB has stated that it appears that the 25% VAT rating applies to all amateur radio equipment and components . . . The recent use of the callsign GB2IARU at Tonbridge School to mark the 50th anniversary of the formation of the IARU is believed to be the first time a four-letter callsign suffix has been authorised for amateur radio operation in the UK . . . During 1976, the bicentennial year of the constitution of the United States, American amateurs will be able to use callsigns beginning with an "A" instead of "W" or "K": all prefixes will have two letters before the district number, ranging from AA1 to AL7 and including AC4 which was formerly used by amateur stations in Tibet and thus one of the most eagerly sought after prefix of all time . . . American amateurs are concerned that a Dallas consulting firm has filed a proposal with the FCC for a new television channel that would result in the elimination of the 50MHz amateur band . . . A 10GHz beacon station at a temporary site on the Isle of Wight has been heard at distances up to 65km, the beacon uses an 80mW oscillator on 10,100  $\pm$  1MHz with an omnidirectional aerial with a gain of about 11dB. Callsign is GB3IOW . . . Among forthcoming mobile rallies are: Longleat near Warminster on June 29 by Bristol RSGB Group; Upton by Worcester society on July 6; Cornish RAC Rally, Camborne (provisional) on July 20 (details G3NKE); Polegate Steam Engine Rally on July 20 with exhibition station GB2SS.

PAT HAWKER, G3VA



# 75 Years of magnetic recording

## 5 — A diversity of applications

by Basil Lane

*Assistant Editor, Wireless World*

**Shortly after the end of World War II, events took an unexpected turn for magnetic recording. Up to that time, although other uses had been suggested for this versatile storage method, the technology had not developed to the stage where they could be practically realized. However, the war effort had resulted in new electronic techniques becoming available and at the same time magnetic recording itself came of age. From that date forward, the number of applications for magnetic recording were to multiply.**

Curiously, for the historian, the task of recording events in the recent past becomes more difficult the closer one approaches the present day. There could be many reasons for this, but in the case of magnetic recording it is because technology from 1945 advanced at such a rate that new developments followed one another at an incredible pace. This makes it difficult to say at times who was first in the field with a particular idea. One can only hope to describe from contemporary reports what happened.

A typical example is the computer. Where now we can hardly think of a computer without also thinking of the magnetic storage methods used, the earliest computers were without such an advantage. Suddenly, everyone seemed to be working on the idea of using magnetic tape as a storage medium. In an historical broadsheet put out by 3M a few years ago<sup>68</sup> it was suggested that flexible storage systems were one of the most significant steps taken by computer designers, and in the days just after the war a variety of memory devices were proposed including delay lines filled with gin!

Just about the earliest computer with a magnetic store was the ARC (Automatic Relay Calculator) made at Birkbeck College, London in 1947. Built for the British Rubber Research Association, it had a nickel plated drum store with a capacity for 256 numbers each of 21 binary digits. Shortly after, the experience gained in developing this computer was used to develop the SEC (Simple Electronic Computer), the first all-electronic computer with a drum store.

Also in 1947, Eckert and Mauchly built a machine called BINAC for the

Northrop Corporation, this computer using a mercury delay-line memory of 512 words and being the first to use a magnetic tape input and output.

Although magnetic drum and disc scored for short term storage with fast, random access, there was an increasing requirement for long term serial data stores of greater versatility than the punched paper tape and card type. Thus in the early 1950s several machines appeared with a tape storage system, one such machine being the IBM 701. This was the first of the IBM machines to use a combined drum and tape store, supplemented with Williams tubes to give a total memory capacity of 2048 words.

Most of the development from that time on, concentrated on the improvement of the magnetic media, not only to reduce the error rate due to drop-outs but also to increase the capacity of the media to record digital bits. Thus the capability rose from 100 bits per square inch in 1947 to 1500 in 1965<sup>69</sup> and as high as 6500 bits per square inch today — although there are at the moment few, if any, machines that are capable of recording such a bit density. Although

plated metal discs had been used from time to time, the real development of this form of recording medium did not start until Zaponi<sup>70</sup> developed a reliable plating technique in 1952. It is interesting to note that 46 years earlier, P. O. Pedersen had patented<sup>71</sup> a plated magnetic carrier though this was of course intended for audio recording.

In modern computers a variety of storage media is used, with magnetic methods still paramount. Disc is used for random access and usually is manufactured as a pack of discs in a standard format. The magnetic layer may be acicular Fe<sub>2</sub>O<sub>3</sub>, plated nickel-cobalt or other similar magnetic metals and the writing and reading are achieved by flying heads located in the appropriate position in the disc pack by high speed actuators. Magnetic tape is still strongly favoured for long term storage where access time is not so important and will be either ferric oxide, cobalt-doped ferric oxide or chromium dioxide, all of the latter having been developed from the early sixties.

The most popular material used in magnetic tapes is still the leader, this being gamma ferric oxide. Since the

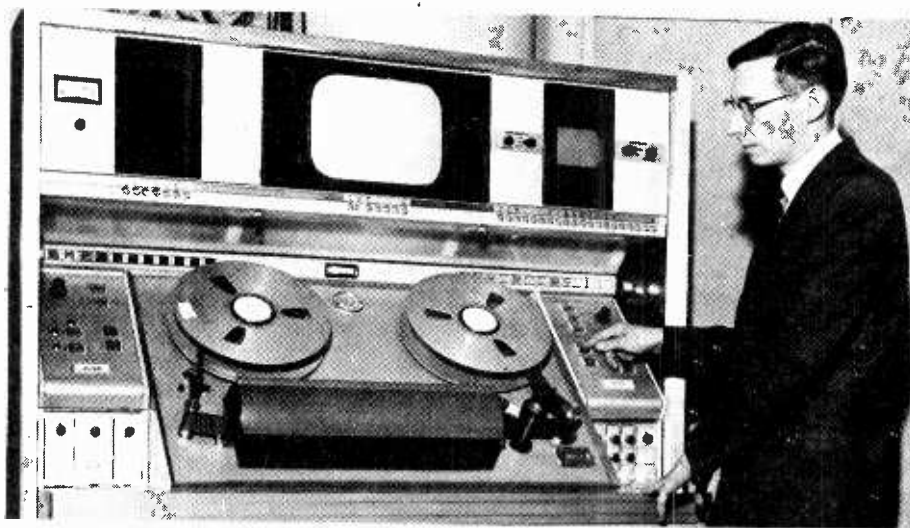


Fig. 2. The TR-22 video recorder by RCA, this was the first transistorized video recorder to enter service, May 7, 1961.

early days of its use as the basis for a coating formulation for magnetic tape, it has been improved and the coating formulation itself developed almost beyond recognition. However, it was inevitable that some challenge to the supremacy of ferric oxide should come from other materials and the demands placed on magnetic tape by the invention of the video recorder and the data recorders for computers provided the impetus for this to happen during the 1960s. From around 1956, cobalt doping of ferric oxide had been studied as a method of improving the short wavelength response of tape and by 1967 an experimental tape had been made. However, the problems associated with this type of magnetic material (e.g. pressure instability of magnetisation) prevented it from becoming as popular as more conventional coatings.

Another line of research had been undertaken by Swoboda<sup>72</sup> who had been concentrating on the problem of synthesizing chromium dioxide, a promising material for tape since it had a high remanence, which offered a very good short wavelength performance. In early 1961 this substance was produced successfully, though it was to be some time before it made its debut as a magnetic tape. As a matter of interest, it took ten years for CrO<sub>2</sub> to appear in a compact cassette, when Crolyn (the Du Pont name for CrO<sub>2</sub>) appeared under labels such as Advent and Memorex.

It is interesting to note that, due to a quirk of American Patent law which allows applications to be patented as well as processes, Du Pont held the master patent for the use of CrO<sub>2</sub> as a magnetic recording medium in America. Process patents are held in all the other countries of the world where applications are not patentable, and it was this situation that led to Agfa Gevaert trying to circumvent the Du Pont patent in 1972. They too had invented a process for the manufacture of CrO<sub>2</sub>, which differed from the Du Pont method, but were prevented from selling any tape in America because of the patent held by Du Pont. The ridiculous situation of being barred from one of their important markets eventually forced Agfa to take out a licence for the Du Pont process and pay for the privilege of selling CrO<sub>2</sub> tape in America.

Since the date of the appearance of CrO<sub>2</sub> as a magnetic medium for cassette tapes, other manufacturers and those who were licencees have been attempting to either equal the performance of this substance, using cheaper ferric oxide, or have been busy looking at other substances. One development that appeared to result from a parallel, but separate, development project was the dual layer coated tape. These had been proposed as early as 1953, when Kornei<sup>74</sup> suggested that short wavelength performance could be improved if a multi-layer tape was prepared with a high coercivity surface layer, followed

with successively deeper layers using oxide of a lower coercivity. Another quite novel idea proposed by Gabor and Bauer<sup>74</sup> was that a dual layer tape should be made with the top layer oriented in a vertical direction.

However, it was Sony and 3M that eventually produced a practical dual layer tape, with Sony marketing its product in Japan in January 1974 and, later that same year, 3M announcing its own product. Again, it would seem that the master patent is probably held in America by 3M,<sup>75</sup> so it is highly likely that Sony have had to come to some cross-licence agreement with 3M in order to sell their tape in the USA.

### Developments in heads

No history of magnetic recording would be complete (and this one is far from being so) without a mention of the development of ferrite heads. With the appearance of CrO<sub>2</sub> tape, which is a much more abrasive material, there was a particular requirement for a hard wearing head to be produced which would withstand many hours of use. This was very important in video recording where the head to tape speed is high and the track width is narrow.

Early heads had been made of laminated Mumetal and although experiments had been made with harder materials such as Alfenol, this proved, until recent years, too intractable to be used as a substitute. Permalloy and other harder grades of metal have been used with increasing success, but it was the ferrite head that made the big news when it was first developed. One of the first descriptions of a ferrite head appeared<sup>76</sup> in 1955, to be followed some years later by the classic paper by S. Duinker<sup>77</sup> of Philips, who described the method of using glass as a spacer and as a bonding material in the front gap of the head. This was a significant improvement that reduced the number of rejected heads that had suffered from chipping at the gap edges.

By 1968, Matsushita had developed the hot pressed ferrite head and about this same time Akai appeared with a glass-crystal ferrite head, made from a monocrystalline block of ferrite.

Other important head types used in specialist fields were the flux sensitive heads, either using a saturable limb in the magnetic circuit of the head, or the semiconductor Hall effect types described by Camras in the mid-1950s. It was Camras also that invented the cross-field head<sup>78</sup> for audio use, this being described January 1952.

In recent years there has been an increasing interest in the fabrication of very precisely defined narrow track heads and to this end experiments have been undertaken to produce sputtered film<sup>79</sup> cores in 1967 and later, in 1972, sputtered film heads using Sendust as the magnetic material.<sup>80</sup>

### Conclusion

In as brief a series as this has been it is difficult to be as thoroughgoing as perhaps one should be, and I am certain that some important inventions have been left out. Little has been said of the p.c.m. recorders developed by the BBC<sup>81</sup>, Nippon Columbia<sup>82</sup> and others<sup>83</sup>, nor has anything of note been mentioned of instrumentation recorders, including those used in the space effort. There are also the more exotic types of recorders such as the brilliant invention by Seimens<sup>84</sup> of the slow and stop motion video disc recorder. However, I feel that all of the significant stages in the development of magnetic recording on the broad front have been covered.

It still seems remarkable that only 75 years ago Poulsen and Pedersen could have been responsible for the whole chain of ideas and inventions that resulted in the magnetic recording process that so invades the everyday life of every one of us.

My apologies to Mrs Pedersen who was kind enough to write and point out an error in spelling P. O. Pedersen's name in earlier parts of this series.

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# New Products

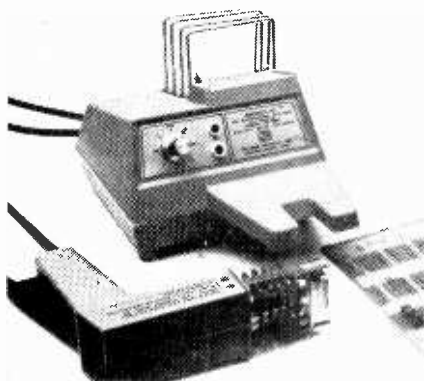
## Thick-film amplifier

A thick-film hybrid amplifier suitable for audio applications will deliver around 15W (average) into an 8Ω load. The class B quasi-complementary circuit has a frequency response from 0 to 80kHz, an input sensitivity of 350mV (typical), and a t.h.d. figure of 0.2%. The device is mounted on an integral heat sink measuring 30 x 30mm which allows full rated output at a temperature of 55°C. Tadiran, 193 Regent Street, London W1.

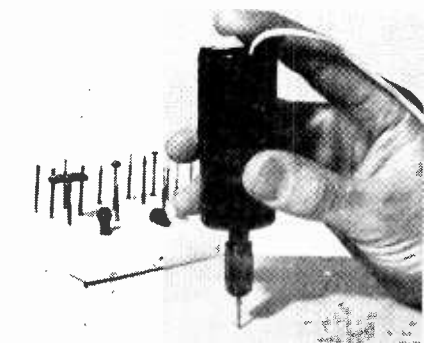
**WW 312 for further details**

## De-soldering instrument

Adcola Products have introduced an automatic de-soldering instrument for removing d.i.l. i.c.s from p.c. boards. The unit, which is called the Removic, consists of an operating gun powered from a control box which adjusts the temperature from 350 to 750°F. In



**WW308**



operation the gun is placed over an i.c., a handle is pressed which positions extractor claws and heater blocks on the i.c. When the solder melts the component is extracted by applying steady pressure on the handle. Adcola Products Ltd, Adcola House, Gauden Road, London SW4.

**WW308 for further details.**

## Mini drill

A small power drill manufactured by Expo operates from a 12V 1A supply and has a chuck speed of around 9000 r.p.m. The drill, which is supplied with a range of accessories which include twist drills, cutting, milling, reaming and grinding tools, is priced at £9.17 plus v.a.t. and is available from Electroplan Ltd, P.O. Box 19, Orchard Road, Royston, Herts SG8 5HH.

**WW310 for further details**

## Alarm unit

The Tellit is an audible alarm unit using a continuous loop of tape which may be recorded with any short message or warning specified by the user. Four basic types are available including an uncased playback mechanism for mounting into customers equipment. Highland Electronics Ltd, 33 Dallington Street, London EC1V 0DB.

**WW311 for further details**

## Counter

A 75-MHz counter/timer, model 5308A, measures frequency, frequency ratio, period, period average, and time inter-

val. The instrument also offers an auto-range facility which selects the range that will give the best resolution within a measuring time from 0.11 to 1.1s. Measurements are indicated by an eight-digit display housed in a 3½ x 6¼ x 9¾in case. Hewlett-Packard Ltd, King Street Lane, Winnersh, Wokingham, Berks RG11 5AR.

**WW303 for further details**

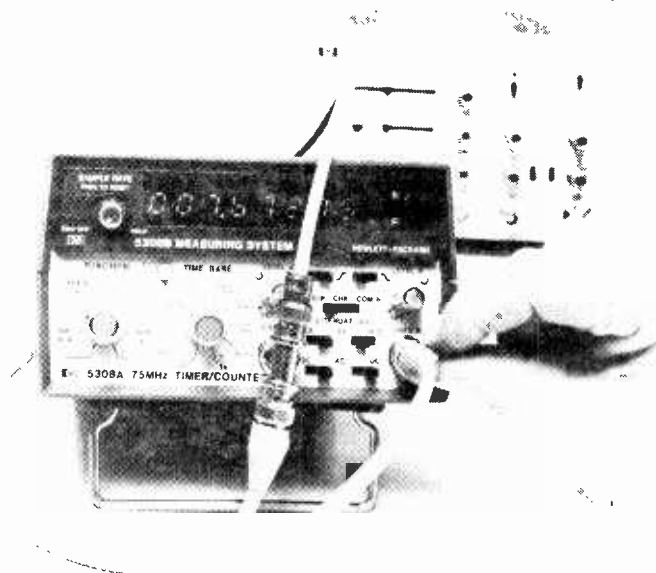
## Triacs

ITT Semiconductors have made their first step into the triac market by announcing the TC range of devices. These components, which have been designed and manufactured in the UK, are available with current ratings of 4, 6, 8, 10, 12 and 16A at voltages of 200, 400, 500 and 600V. The complete range uses a centre-gate construction for improved  $di/dt$  capability, and has glass passivated chips which improve high-voltage protection. All of the devices are housed in the TO-220AB plastic package and are priced between £0.416 and £1.88 each depending on type and quantity. ITT Semiconductors, Foots Cray, Sidcup, Kent.

**WW 335 for further details**

## Microwave coupler

Walmore are now supplying the Norsal 4834 microwave coupler. This device, which is claimed to be the first to cover the range 2 to 12.4GHz, has a v.s.w.r. of 1.4:1, amplitude imbalance of  $\pm 0.5$ dB, and a phase imbalance of  $\pm 7^\circ$ . The coupler is designed to handle input powers of 20W average with a 2kW



**WW303**

**WW310**



WW302



WW313



WW309

peak rating. Microwave Division, Walmore Electronics Ltd, 11 Betterton Street, London WC2H 9BS.

**WW307 for further details**

### Variable-filters

The EF3/03 and EF3/04 are recent additions to the Barr & Stroud range of variable filters. The units are high-pass and low-pass filters respectively which may be switched into several modes including band-pass and band-stop. The cut-off frequency is variable from 0.1Hz to 100kHz with a stop-band attenuation rate of 48dB/octave and a pass-band response from 0 to 700kHz. Barr & Stroud Ltd, Kinnaird House, 1 Pall Mall East, London SW1Y 5AU.

**WW302 for further details**

### Signal generator

The Fluke synthesized signal generator, model 6010A offers a keyboard entry with a manual fine control, and a built-in microprocessor which can store up to nine programmes. Each programme consists of a frequency, a frequency range, an amplitude, and a modulation (c.w., a.m., or f.m.). These programmes can be recalled at any point in a testing sequence. The instrument has a frequency range from 10Hz to 109kHz in 0.1Hz steps and 10Hz to 10MHz in 10Hz steps, an accuracy of  $\pm 3$  parts in  $10^6$  in the temperature range 0 to  $+50^\circ\text{C}$  and a variable output level from 0.25mV to 5V r.m.s. The selected frequency is indicated on a seven-digit l.e.d. display. Fluke (Nederland) B.V., Ledeborstraat 27, Tilburg, Netherlands.

**WW313 for further details**

### Testing system

The type 8309 test set connects directly to a computer terminal and will transmit to, or receive messages from the terminal for the purpose of checking and/or fault analysis. The 8309 can be operated at data rates between 110 and 9600 bits/sec in a synchronous or asynchronous mode. In the former mode it responds to either the EBCDIC or ASCII SYN character set, while in the latter case the number of stop bits sent by the transmitter may be selected as required. Data Recognition Ltd, Loverock Road, Battle Farm Estate, Reading, Berks.

**WW309 for further details**

### Bezel

A recent addition to the Roxburgh range of switches and accessories is a bezel incorporating a l.e.d. mounting facility. The bezel fits the J50, J60 and 800J switches and accepts a 0.2in l.e.d. Roxburgh Electronics Ltd, 22 Winchelsea Road, Rye, Sussex.

**WW301 for further details**

# Products seen at Hi-Fidelity 75

## Sansui tuner

The TU-7700 stereo tuner is one of a series of amplifiers and tuners which Sansui have added to their range. This model will receive f.m. broadcasts within the frequency range 88-108MHz and a.m. broadcasts in the range 535-1605kHz. Containing a high integrated-circuit count, the TU-7700 is to retail at a suggested price of £149.10 plus VAT. Vernitron Ltd, Thornhill, Southampton SO9 5QF.

## Four-channel tape deck

Well known on the Continent, but new to the UK, the Dokorder range of reel-to-reel recorders is being distributed by Acoustico Enterprises. The top of the domestic range is the model 7140 which is fully equipped to record and replay up to four tracks on 1/4in tape. The head block is interchangeable to offer two track stereo recording and a consequent improvement in signal-to-noise ratio.

A useful facility is offered by the so-called "Multi-Sync" which is a switching arrangement which connects one or more record head tracks to the replay amplifier to permit monitoring of previously recorded tracks, whilst adding in synchronism further recordings to remaining free tracks.

Other facilities include sound-on-sound, echo, bias and record equalisation for two types of tape and A-B monitoring. Acoustico Enterprises Ltd, Unit 7, Space Way, North Feltham Trading Estate, Feltham, Middx TW14 0TZ.

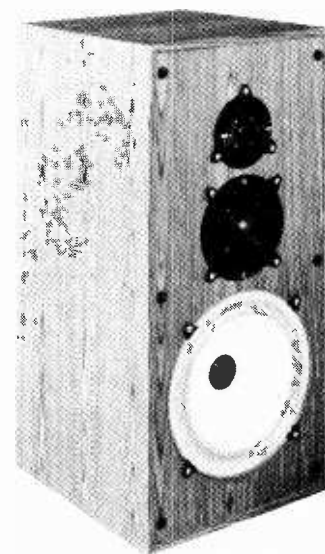
## Eagle range

Eagle International have added considerably to their range of products with the introduction of the 2000 series of equipment. This comprises the A2004 and A2006 amplifiers with a rated output of 20W per channel and having a rather more complex range of tone controls than usual. A matching tuner amplifier, the A2008, provides for reception of the a.m. and f.m. bands and

also there is a synchronous motor, belt drive turntable, the D2005. A second turntable, the D2006, is classified by Eagle as a servo-monitor type, though exactly what this means is not quite clear. Finally the 2000 series is completed by a choice of five loudspeakers and two headphones. Eagle International, Heather Park Drive, Wembley, Middx HA0 1SU.

## New belt drive turntables

The BDS80 and BDS90 are two turntables added to the series produced by BSR McDonald. Both models are semi-automatic in that when a record has finished playing the arm lifts up, returns to rest, locks and switches off. Both decks are also fitted with a click suppressor and muting switch which prevent an unwanted noise being fed to the amplifier while the automatic set-down and switch off are in operation. A special feature of the BDS90, according to the manufacturers is a new low-resonance tubular aluminium tone-arm, located in a concentric gimbal style mount which carries a calibrated stylus pressure control. The rumble figure for both units is stated to be 55dB. Standard units are available for either 100-125V 60Hz or 200-240V 50Hz. BSR Ltd, Monarch Works, Cradley Heath, Warley, Worcs.



## Three new speakers

A new range of loudspeakers from Celestion are the UL6, UL8 and UL10 models. The two smaller models in the range are both two-unit systems, the bass driver being supplemented by a passive auxiliary bass radiator unit. The largest model is the UL10 (see photograph) which houses three in-line drive units. Cabinet dimensions are 673mm height, 317mm width, 380mm depth. Power handling is rated at 50W continuous or 100W peak music power. Sensitivity is sensibly rated using pink noise, an input of 12 volts r.m.s. being required to produce 96dB s.p.l. at 1 metre. Frequency response is stated to be 40Hz to 20kHz  $\pm$ 2dB. Drive units consist of the HF2000 super tweeter, the MD7000 pressure-dome mid range unit and a 254mm bass drive unit. Rola Celestion Ltd, Ditton Works, Foxhall Road, Ipswich, Suffolk IP3 8JP.

## New life for Wharfedale

Rank Radio introduced a new XP range of speakers carrying the well-known names of Denton, Linton and Glendale. All have greater power handling capability and are claimed to have improved performance over their predecessors. Taking the smallest in the range, the Denton 2XP, this is a two-way bookshelf enclosure of acoustic suspension



Sansui Tu-7700 stereo tuner



design. Main specifications are: power handling 25W (DIN), suitable for use with amplifiers rated from 3 to 30W continuous; frequency response 65-17kHz at -3dB points; crossover frequency 1.4kHz; sensitivity is 96dB at 1m for 6W input; impedance is 6Ω nominal; dimensions are 355 × 246 × 22mm. Finish is in teak or white. Rank Radio International Ltd, P.O. Box 596, Power Road, London W4 5PW.

## Amplifier with limiter circuit

The new Cambridge Classic One amplifier has several unusual features including l.e.d. monitoring of pre-amplifier signal level in 5dB steps. An l.e.d. indicator is used as a power supply indicator. This also flashes at a regular rate whenever a power amplifier limiter circuit is brought into operation. A circuit in conjunction with the input selector switch is provided to limit the effect of switch-on transients causing 'thumps' through the loudspeakers. Main specifications are: power output at 1kHz, 60W per channel into 8Ω; t.h.d. is less than 0.05% at all audio frequencies, typically 0.005%; signal-to-noise ratio is 65dB ref. 2mV (pickup input), 75dB ref. 250mV (line inputs); input sensitivities are pickup 2mV/47kΩ, tuner 250mV, cassette 100mV and auxiliary 100mV. The pickup input overload capability is rated at 45dB. Facility for the simultaneous use of three tape recorders is also provided. Cambridge Audio Ltd, Lamb House, Church Street, London W3 2PB.

## Solid State Devices

Names of suppliers of devices in this section are given in abbreviation after each entry and in full at the end of the section.

### Shift register

A 512-bit dynamic shift register with built-in recirculating and command logic has a maximum operating speed of 4MHz.

**WW350 for further details** G.E.

### Diodes

The 501PD series of diodes has an average current rating of 500A at an 84°C case temperature, and are available over the voltage range 2kV to 4kV with non-repetitive ratings up to 4.4kV.

**WW351 for further details** I.R.

### R.a.m.

The 1103-1 is a 1k dynamic r.a.m. offering a 340ns full-cycle time and a 150ns read access time. All address inputs are fully decoded and typical power dissipation is 0.4mW/bit.

**WW352 for further details** ITT

### Schottky register

A 4-bit register having three-state and standard t.t.l. outputs has been built using Schottky technology. The device is available in three packages and is priced from \$3.08 100 up.

**WW353 for further details** AMD

### Programmable op-amp

Parameters of the MC3476 op-amp are programmed by an external resistor to suit power supplies from ±6 to ±15V. The device does not require frequency compensation, has offset null capability and is protected against short circuits.

**WW354 for further details** Motorola

### Bridge rectifiers

A new range of bridge rectifiers has a built-in capacitor in parallel with each diode to absorb reverse voltage transients. The range has repetitive peak-reverse voltage ratings from 50 to 600V and an average direct current rating of 2A.

**WW355 for further details** ME

### Memory driver

An n-channel m.o.s. memory driver i.c., type MC3459, contains four identical driver circuits and is capable of maintaining a propagation delay of 20ns when driving a 360pF load.

**WW 356 for further details** Motorola

### A-to-d converter

The MC904 is claimed to be the first monolithic i.c. with all the functions necessary for a digital panel meter or multimeter. The device has a resolution of 100μV and an input impedance of 1000MΩ and is housed in a 28-pin d.i.l. package.

**WW358 for further details** Macro

### Image sensor

A new 1728-element charge-coupled linear image sensor, suitable for use in optical page scanning systems, has been introduced by Fairchild. The CCD121 is capable of reading a standard 8½ × 11-inch page in less than one second and up to 200 lines per inch can be resolved.

**WW 359 for further details** Fairchild

### Count/display i.c.

A t.t.l.-compatible universal count/display i.c., type ZN1040E, offers a count rate of over 5MHz. The device requires a 5V supply and is housed in a 28 pin d.i.l. package.

**WW360 for further details** Ferranti

### Low-voltage sensor

An i.c. intended for use with battery operated equipment, is internally set to trigger when a voltage drops to 2.4V ±2%. This value can be increased by adding a resistor.

**WW361 for further details** Bowmar

### Sample/hold amp

An adjustment-free sample/hold amplifier called the MN343 provides a droop rate of less than 0.3mV/ms and an acquisition time of better than 10μs.

**WW 362 for further details** Tranchant

### F.e.t. input amplifier

The 3670 is a f.e.t.-input i.c. instrumentation amplifier. Gain adjustment, from 1 to 1000V/V, is made with one resistor. Maximum bias current is 10pA, and the input impedance is 10<sup>13</sup> ohms.

**WW363 for further details** Burr Brown

**G.E. Electronics** (London) Ltd, 182/4 Campden Hill Road, Kensington, London W8 7AS.

**International Rectifier**, Hurst Green, Oxted, Surrey RH8 9BB.

**ITT Semiconductors**, Footscray, Sidcup, Kent.

**Advanced Micro Devices Inc.**, 901 Thompson Place, Sunnyvale, California 94086, U.S.A.

**Motorola Ltd**, Semiconductor Products Division, York House, Empire Way, Wembley, Middx.

**Micro Electronics Ltd**, York House, Empire Way, Wembley, Middx.

**Macro Marketing Ltd**, 396 Bath Road, Slough, Bucks.

**Fairchild Camera & Instrument Corporation**, Northway House, High Road, Whetstone, London N.20.

**Ferranti Ltd**, Electronic Components Division, Gem Mill, Chadderton, Oldham, OL9 8NP.

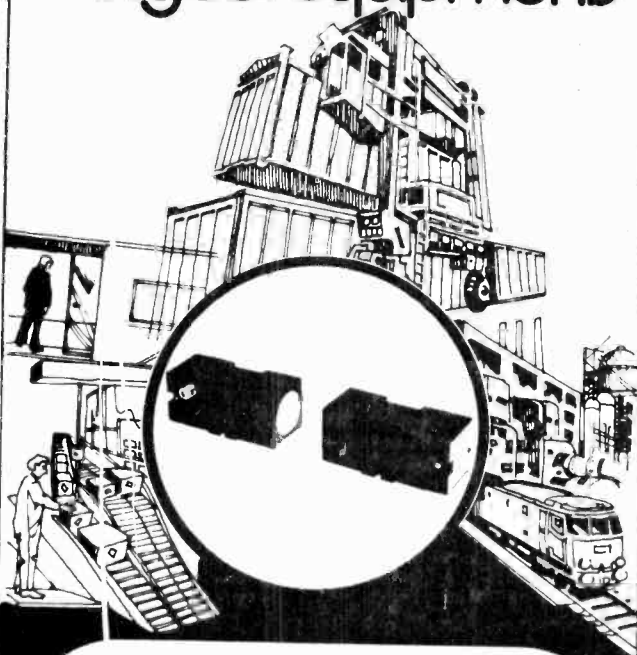
**Bowmar Arizona, Inc.**, 2355 West Williams Field Road, Chandler, Arizona 85224, U.S.A.

**Tranchant Electronics (UK) Ltd**, Tranchant House, 100a High Street, Hampton, Middx.

**Burr-Brown International**, 25a King Street, Watford, WD1 8BT.

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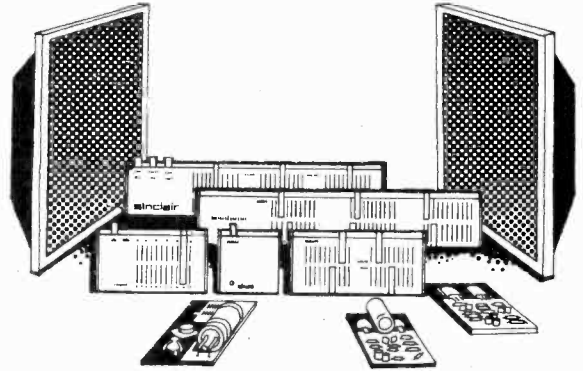


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WW-007 FOR FURTHER DETAILS

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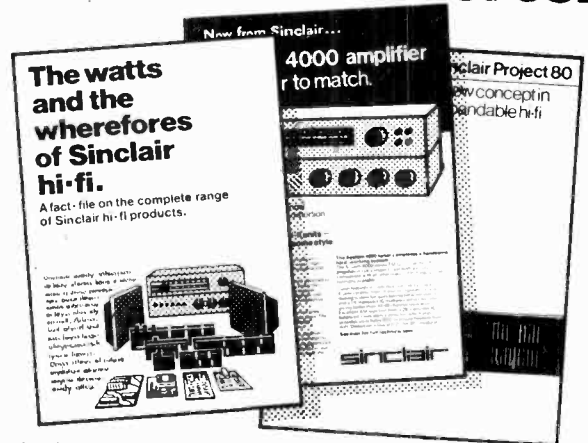
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in easy-to-work blue and white PVC/steel. Assemble in the lower half complete before springing cover into place—four Pozidrivs, two to hinge it, two to fasten it. Carries four PC boards horizontally, or two vertically, four required for each case (for one vertical board, two each case) Prices correct May 1975

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Much less for quantity. Prices include P & P 8% VAT, four feet and four plated screws. Special feet to carry Printed Circuit Boards sold separately. Price, incl. 8% VAT, 25p for four PC feet

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Contil Mod-3 cases are in six sizes and offer the manufacturer of small instruments an attractive low cost case available ex-stock. Made in blue PVC-coated steel and complete with front and rear panels and chassis, they are light, strong and rigid. PCB and PSU mounting systems available

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Mod 303	£6.04		7"		6"		5 1/4"
Mod 304	£6.04		11"		3"		5 1/4"
Mod 305	£7.04		11"		4 1/2"		5 1/4"
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28 SIZES AVAILABLE

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Much less for quantities. Boplast cases are available with clear covers. M210, 221, 223, 233, 244 (suffix G when ordering). Cable glands available. Prices correct May 1975

WEST HYDE NOW HAVE OVER 160 SIZES AND TYPES OF CASES, PLASTIC AND METAL.

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## Heat Sink and Case in One

The front and back heavy extrusions contain slots for mounting power transistors or transformers. Access is by means of the removable side plates which allow the black PVC top and bottom panels to be slid out so providing good access to the interior. With 3/16" thick side removed, the case is still mechanically stiff.

The good-looking Swift case is made of aluminium. Side plates black anodised, the front and rear extrusions satin anodised. Only 8 parts and 8 screws. The feet lock into the case below for stacking.

Full width rack 3 1/2" high	1 off incl P&P and VAT	Size
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# CONTIL MOD-2

The design of these cases permits the instrument to be built or serviced within their external panels. 48 shapes. Low cost. Blue PVC/steel with grey PVC-coated aluminium panels.

Width	Height	Depth	1 off	Width	Height	Depth	1 of
A 4 1/2"	3"	6 1/2"	£4.67	M 4 1/2"	7"	13"	£5.50
B 4 1/2"	7"	6 1/2"	£5.50	N 4 1/2"	7"	13"	£7.35
C 4 1/2"	10"	6 1/2"	£6.68	O 4 1/2"	10"	13"	£9.69
D 9"	6 1/2"	6 1/2"	£6.68	P 9"	3"	13"	£7.35
E 9"	7"	6 1/2"	£7.35	Q 9"	7"	13"	£9.69
F 9"	10"	6 1/2"	£8.67	R 9"	10"	13"	£11.92
G 13"	3"	6 1/2"	£7.35	S 13"	3"	13"	£9.69
H 13"	7"	6 1/2"	£8.67	T 13"	7"	13"	£11.92
I 13"	10"	6 1/2"	£9.69	U 13"	10"	13"	£15.78
J 18"	3"	6 1/2"	£8.67	V 18"	3"	13"	£11.92
K 18"	7"	6 1/2"	£11.92	W 18"	7"	13"	£15.78
L 18"	10"	6 1/2"	£15.78	X 18"	10"	13"	£17.37

Mod-2 in Woodgrain finish in sizes A, B, C, D, E, G, F, H, J, K & L

Prices as for one price up on Mod-2, e.g. Mod 2A Woodgrain is £5.50

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WW 036 FOR FURTHER DETAILS

# ROGERS AUDIO TEST EQUIPMENT



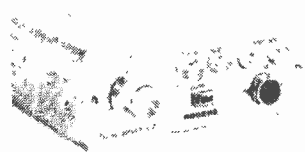
A comprehensive, versatile range of test equipment primarily designed for the measurement of high quality audio equipment but with additional applications in the electronics industry in general. The equipment is of particular interest to the professional audio engineer, recording studios, broadcasting authorities and educational establishments.

**DM344A Distortion Factor Meter.** Designed to make accurate and rapid measurements of total harmonic distortion generated within high quality audio amplifiers, recording and transmission equipment. **Selling Price: c/w Bench Case £175.00 + VAT.**

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**BAILEY/BURROWS/QUILTER PRE AMP** This is the tone control section of the best pre-amp kit currently available. Consider the advantages—\*First quality fibreglass printed circuits with roller tinned finish and all component locations printed on reverse. \*Low noise carbon film and metal film resistors throughout. \*Finest quality low noise ganged controls with matched tracks and shafts cut to length. \*Well engineered layout for total stability. \*Special decoupling and earthing arrangements to eliminate hum loops. \*Controls, switches and input sockets mount directly on the boards to TOTALLY ELIMINATE wiring to these components. (We know of one pre amp kit which claims its controls mount directly on the board—and so they do, by their shaft bushes! You still have to wire them up!)

\*We incorporate the Quilter modification which is most important as it reduces distortion and increases the bass and treble control range.

As can be seen from the photograph the tone control unit is very slim (only 1 1/2" from front to back) and may therefore be used in many other applications than our Bailey metalwork which it is designed to fit.

**METALWORK AND WOODEN CASES** These have been under review for some time please send for latest information.

**F.M. TUNER** This latest addition to our range is designed to offer the best possible performance allied to the ease of operation given by push button varicap tuning. We have taken great care to look after the constructors point of view and there are no coils to wind, no RF circuits to wire and no alignment is required. In fact the whole unit and two ready built aligned modules comprising the active components. We have abandoned the concept of having a tuner as large as the amplifier as this new unit has a frontal size of only 1 1/2" x 4 in. It can be mounted on the side of our Bailey amplifier metalwork thus turning it into a tuner/amplifier whilst only increasing its width by 1 1/2 in. Cost of tuner chassis (no case) is £22 for mono. £25.45 for stereo. Metal case £35.50. An extended wooden case to fit tuner and amplifier will be offered shortly.

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# More than just a catalogue!

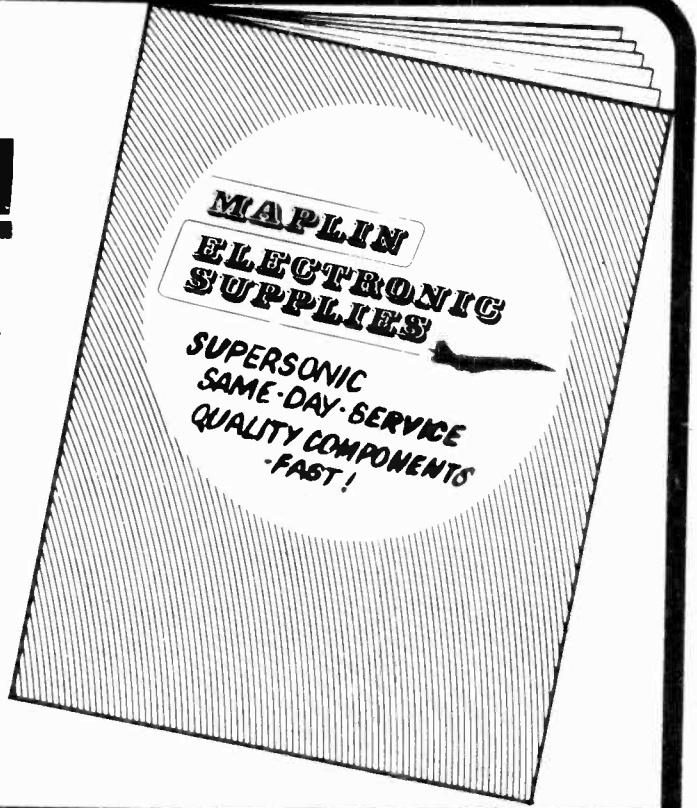
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CIRCUITS . . . Frequency Doublers, Oscillators, Timers, Voltmeters, Power Supplies, Amplifiers, Capacitance Multiplier, etc., etc. . . .

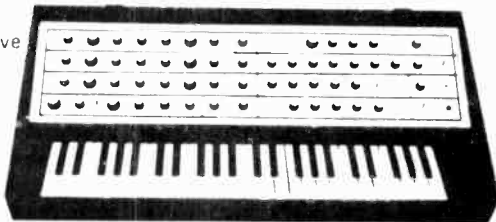
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Really good value for money at just 40p.



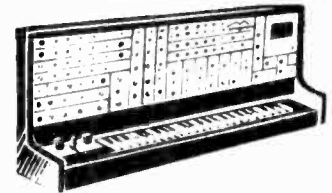
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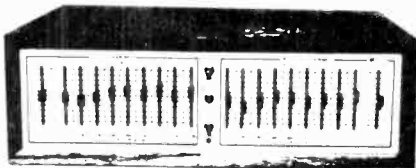
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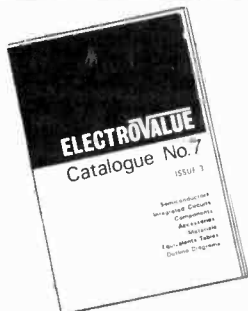
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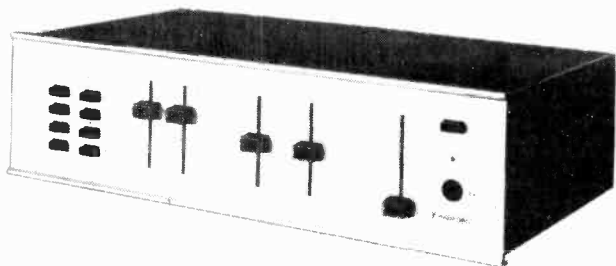
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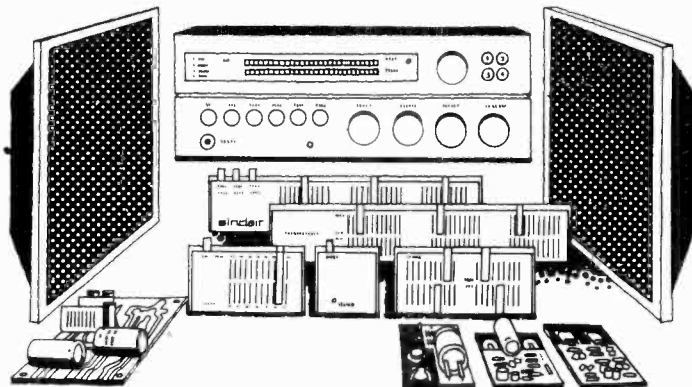
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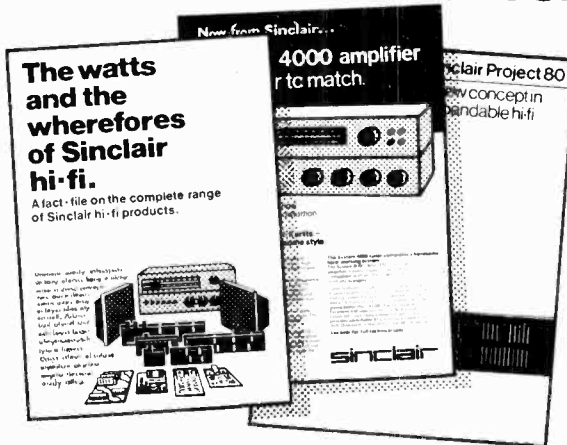
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### VALVES

EAZ13	0.70	EAZ14	0.80	EAZ15	0.90	EAZ16	1.00	EAZ17	1.10	EAZ18	1.20	EAZ19	1.30	EAZ20	1.40	EAZ21	1.50	EAZ22	1.60	EAZ23	1.70	EAZ24	1.80	EAZ25	1.90	EAZ26	2.00	EAZ27	2.10	EAZ28	2.20	EAZ29	2.30	EAZ30	2.40	EAZ31	2.50	EAZ32	2.60	EAZ33	2.70	EAZ34	2.80	EAZ35	2.90	EAZ36	3.00	EAZ37	3.10	EAZ38	3.20	EAZ39	3.30	EAZ40	3.40	EAZ41	3.50	EAZ42	3.60	EAZ43	3.70	EAZ44	3.80	EAZ45	3.90	EAZ46	4.00	EAZ47	4.10	EAZ48	4.20	EAZ49	4.30	EAZ50	4.40	EAZ51	4.50	EAZ52	4.60	EAZ53	4.70	EAZ54	4.80	EAZ55	4.90	EAZ56	5.00	EAZ57	5.10	EAZ58	5.20	EAZ59	5.30	EAZ60	5.40	EAZ61	5.50	EAZ62	5.60	EAZ63	5.70	EAZ64	5.80	EAZ65	5.90	EAZ66	6.00	EAZ67	6.10	EAZ68	6.20	EAZ69	6.30	EAZ70	6.40	EAZ71	6.50	EAZ72	6.60	EAZ73	6.70	EAZ74	6.80	EAZ75	6.90	EAZ76	7.00	EAZ77	7.10	EAZ78	7.20	EAZ79	7.30	EAZ80	7.40	EAZ81	7.50	EAZ82	7.60	EAZ83	7.70	EAZ84	7.80	EAZ85	7.90	EAZ86	8.00	EAZ87	8.10	EAZ88	8.20	EAZ89	8.30	EAZ90	8.40	EAZ91	8.50	EAZ92	8.60	EAZ93	8.70	EAZ94	8.80	EAZ95	8.90	EAZ96	9.00	EAZ97	9.10	EAZ98	9.20	EAZ99	9.30	EAZ100	9.40	EAZ101	9.50	EAZ102	9.60	EAZ103	9.70	EAZ104	9.80	EAZ105	9.90	EAZ106	10.00	EAZ107	10.10	EAZ108	10.20	EAZ109	10.30	EAZ110	10.40	EAZ111	10.50	EAZ112	10.60	EAZ113	10.70	EAZ114	10.80	EAZ115	10.90	EAZ116	11.00	EAZ117	11.10	EAZ118	11.20	EAZ119	11.30	EAZ120	11.40	EAZ121	11.50	EAZ122	11.60	EAZ123	11.70	EAZ124	11.80	EAZ125	11.90	EAZ126	12.00	EAZ127	12.10	EAZ128	12.20	EAZ129	12.30	EAZ130	12.40	EAZ131	12.50	EAZ132	12.60	EAZ133	12.70	EAZ134	12.80	EAZ135	12.90	EAZ136	13.00	EAZ137	13.10	EAZ138	13.20	EAZ139	13.30	EAZ140	13.40	EAZ141	13.50	EAZ142	13.60	EAZ143	13.70	EAZ144	13.80	EAZ145	13.90	EAZ146	14.00	EAZ147	14.10	EAZ148	14.20	EAZ149	14.30	EAZ150	14.40	EAZ151	14.50	EAZ152	14.60	EAZ153	14.70	EAZ154	14.80	EAZ155	14.90	EAZ156	15.00	EAZ157	15.10	EAZ158	15.20	EAZ159	15.30	EAZ160	15.40	EAZ161	15.50	EAZ162	15.60	EAZ163	15.70	EAZ164	15.80	EAZ165	15.90	EAZ166	16.00	EAZ167	16.10	EAZ168	16.20	EAZ169	16.30	EAZ170	16.40	EAZ171	16.50	EAZ172	16.60	EAZ173	16.70	EAZ174	16.80	EAZ175	16.90	EAZ176	17.00	EAZ177	17.10	EAZ178	17.20	EAZ179	17.30	EAZ180	17.40	EAZ181	17.50	EAZ182	17.60	EAZ183	17.70	EAZ184	17.80	EAZ185	17.90	EAZ186	18.00	EAZ187	18.10	EAZ188	18.20	EAZ189	18.30	EAZ190	18.40	EAZ191	18.50	EAZ192	18.60	EAZ193	18.70	EAZ194	18.80	EAZ195	18.90	EAZ196	19.00	EAZ197	19.10	EAZ198	19.20	EAZ199	19.30	EAZ200	19.40	EAZ201	19.50	EAZ202	19.60	EAZ203	19.70	EAZ204	19.80	EAZ205	19.90	EAZ206	20.00	EAZ207	20.10	EAZ208	20.20	EAZ209	20.30	EAZ210	20.40	EAZ211	20.50	EAZ212	20.60	EAZ213	20.70	EAZ214	20.80	EAZ215	20.90	EAZ216	21.00	EAZ217	21.10	EAZ218	21.20	EAZ219	21.30	EAZ220	21.40	EAZ221	21.50	EAZ222	21.60	EAZ223	21.70	EAZ224	21.80	EAZ225	21.90	EAZ226	22.00	EAZ227	22.10	EAZ228	22.20	EAZ229	22.30	EAZ230	22.40	EAZ231	22.50	EAZ232	22.60	EAZ233	22.70	EAZ234	22.80	EAZ235	22.90	EAZ236	23.00	EAZ237	23.10	EAZ238	23.20	EAZ239	23.30	EAZ240	23.40	EAZ241	23.50	EAZ242	23.60	EAZ243	23.70	EAZ244	23.80	EAZ245	23.90	EAZ246	24.00	EAZ247	24.10	EAZ248	24.20	EAZ249	24.30	EAZ250	24.40	EAZ251	24.50	EAZ252	24.60	EAZ253	24.70	EAZ254	24.80	EAZ255	24.90	EAZ256	25.00	EAZ257	25.10	EAZ258	25.20	EAZ259	25.30	EAZ260	25.40	EAZ261	25.50	EAZ262	25.60	EAZ263	25.70	EAZ264	25.80	EAZ265	25.90	EAZ266	26.00	EAZ267	26.10	EAZ268	26.20	EAZ269	26.30	EAZ270	26.40	EAZ271	26.50	EAZ272	26.60	EAZ273	26.70	EAZ274	26.80	EAZ275	26.90	EAZ276	27.00	EAZ277	27.10	EAZ278	27.20	EAZ279	27.30	EAZ280	27.40	EAZ281	27.50	EAZ282	27.60	EAZ283	27.70	EAZ284	27.80	EAZ285	27.90	EAZ286	28.00	EAZ287	28.10	EAZ288	28.20	EAZ289	28.30	EAZ290	28.40	EAZ291	28.50	EAZ292	28.60	EAZ293	28.70	EAZ294	28.80	EAZ295	28.90	EAZ296	29.00	EAZ297	29.10	EAZ298	29.20	EAZ299	29.30	EAZ300	29.40	EAZ301	29.50	EAZ302	29.60	EAZ303	29.70	EAZ304	29.80	EAZ305	29.90	EAZ306	30.00	EAZ307	30.10	EAZ308	30.20	EAZ309	30.30	EAZ310	30.40	EAZ311	30.50	EAZ312	30.60	EAZ313	30.70	EAZ314	30.80	EAZ315	30.90	EAZ316	31.00	EAZ317	31.10	EAZ318	31.20	EAZ319	31.30	EAZ320	31.40	EAZ321	31.50	EAZ322	31.60	EAZ323	31.70	EAZ324	31.80	EAZ325	31.90	EAZ326	32.00	EAZ327	32.10	EAZ328	32.20	EAZ329	32.30	EAZ330	32.40	EAZ331	32.50	EAZ332	32.60	EAZ333	32.70	EAZ334	32.80	EAZ335	32.90	EAZ336	33.00	EAZ337	33.10	EAZ338	33.20	EAZ339	33.30	EAZ340	33.40	EAZ341	33.50	EAZ342	33.60	EAZ343	33.70	EAZ344	33.80	EAZ345	33.90	EAZ346	34.00	EAZ347	34.10	EAZ348	34.20	EAZ349	34.30	EAZ350	34.40	EAZ351	34.50	EAZ352	34.60	EAZ353	34.70	EAZ354	34.80	EAZ355	34.90	EAZ356	35.00	EAZ357	35.10	EAZ358	35.20	EAZ359	35.30	EAZ360	35.40	EAZ361	35.50	EAZ362	35.60	EAZ363	35.70	EAZ364	35.80	EAZ365	35.90	EAZ366	36.00	EAZ367	36.10	EAZ368	36.20	EAZ369	36.30	EAZ370	36.40	EAZ371	36.50	EAZ372	36.60	EAZ373	36.70	EAZ374	36.80	EAZ375	36.90	EAZ376	37.00	EAZ377	37.10	EAZ378	37.20	EAZ379	37.30	EAZ380	37.40	EAZ381	37.50	EAZ382	37.60	EAZ383	37.70	EAZ384	37.80	EAZ385	37.90	EAZ386	38.00	EAZ387	38.10	EAZ388	38.20	EAZ389	38.30	EAZ390	38.40	EAZ391	38.50	EAZ392	38.60	EAZ393	38.70	EAZ394	38.80	EAZ395	38.90	EAZ396	39.00	EAZ397	39.10	EAZ398	39.20	EAZ399	39.30	EAZ400	39.40	EAZ401	39.50	EAZ402	39.60	EAZ403	39.70	EAZ404	39.80	EAZ405	39.90	EAZ406	40.00	EAZ407	40.10	EAZ408	40.20	EAZ409	40.30	EAZ410	40.40	EAZ411	40.50	EAZ412	40.60	EAZ413	40.70	EAZ414	40.80	EAZ415	40.90	EAZ416	41.00	EAZ417	41.10	EAZ418	41.20	EAZ419	41.30	EAZ420	41.40	EAZ421	41.50	EAZ422	41.60	EAZ423	41.70	EAZ424	41.80	EAZ425	41.90	EAZ426	42.00	EAZ427	42.10	EAZ428	42.20	EAZ429	42.30	EAZ430	42.40	EAZ431	42.50	EAZ432	42.60	EAZ433	42.70	EAZ434	42.80	EAZ435	42.90	EAZ436	43.00	EAZ437	43.10	EAZ438	43.20	EAZ439	43.30	EAZ440	43.40	EAZ441	43.50	EAZ442	43.60	EAZ443	43.70	EAZ444	43.80	EAZ445	43.90	EAZ446	44.00	EAZ447	44.10	EAZ448	44.20	EAZ449	44.30	EAZ450	44.40	EAZ451	44.50	EAZ452	44.60	EAZ453	44.70	EAZ454	44.80	EAZ455	44.90	EAZ456	45.00	EAZ457	45.10	EAZ458	45.20	EAZ459	45.30	EAZ460	45.40	EAZ461	45.50	EAZ462	45.60	EAZ463	45.70	EAZ464	45.80	EAZ465	45.90	EAZ466	46.00	EAZ467	46.10	EAZ468	46.20	EAZ469	46.30	EAZ470	46.40	EAZ471	46.50	EAZ472	46.60	EAZ473	46.70	EAZ474	46.80	EAZ475	46.90	EAZ476	47.00	EAZ477	47.10	EAZ478	47.20	EAZ479	47.30	EAZ480	47.40	EAZ481	47.50	EAZ482	47.60	EAZ483	47.70	EAZ484	47.80	EAZ485	47.90	EAZ486	48.00	EAZ487	48.10	EAZ488	48.20	EAZ489	48.30	EAZ490	48.40	EAZ491	48.50	EAZ492	48.60	EAZ493	48.70	EAZ494	48.80	EAZ495	48.90	EAZ496	49.00	EAZ497	49.10	EAZ498	49.20	EAZ499	49.30	EAZ500	49.40	EAZ501	49.50	EAZ502	49.60	EAZ503	49.70	EAZ504	49.80	EAZ505	49.90	EAZ506	50.00	EAZ507	50.10	EAZ508	50.20	EAZ509	50.30	EAZ510	50.40	EAZ511	50.50	EAZ512	50.60	EAZ513	50.70	EAZ514	50.80	EAZ515	50.90	EAZ516	51.00	EAZ517	51.10	EAZ518	51.20	EAZ519	51.30	EAZ520	51.40	EAZ521	51.50	EAZ522	51.60	EAZ523	51.70	EAZ524	51.80	EAZ525	51.90	EAZ526	52.00	EAZ527	52.10	EAZ528	52.20	EAZ529	52.30	EAZ530	52.40	EAZ531	52.50	EAZ532	52.60	EAZ533	52.70	EAZ534	52.80	EAZ535	52.90	EAZ536	53.00	EAZ537	53.10	EAZ538	53.20	EAZ539	53.30	EAZ540	53.40	EAZ541	53.50	EAZ542	53.60	EAZ543	53.70	EAZ544	53.80	EAZ545	53.90	EAZ546	54.00	EAZ547	54.10	EAZ548	54.20	EAZ549	54.30	EAZ550	54.40	EAZ551	54.50	EAZ552	54.60	EAZ553	54.70	EAZ554	54.80	EAZ555	54.90	EAZ556	55.00	EAZ557	55.10	EAZ558	55.20	EAZ559	55.30	EAZ560	55.40	EAZ561	55.50	EAZ562	55.60	EAZ563	55.70	EAZ564	55.80	EAZ565	55.90	EAZ566	56.00	EAZ567	56.10	EAZ568	56.20	EAZ569	56.30	EAZ570	56.40	EAZ571	56.50	EAZ572	56.60	EAZ573	56.70	EAZ574	56.80	EAZ575	56.90	EAZ576	57.00	EAZ577	57.10	EAZ578	57.20	EAZ579	57.30	EAZ580	57.40	EAZ581	57.50	EAZ582	57.60	EAZ583	57.70	EAZ584	57.80	EAZ585	57.90	EAZ586	58.00	EAZ587	58.10	EAZ588	58.20	EAZ589	58.30	EAZ590	58.40	EAZ591	58.50	EAZ592	58.60	EAZ593	58.70	EAZ594	58.80	EAZ595	58.90	EAZ596	59.00	EAZ597	59.10	EAZ598	59.20	EAZ599	59.30	EAZ600	59.40	EAZ601	59.50	EAZ602	59.60	EAZ603	59.70	EAZ604	59.80	EAZ605	59.90	EAZ606	60.00	EAZ607	60.10	EAZ608	60.20	EAZ609	60.30	EAZ610	60.40	EAZ611	60.50	EAZ612	60.60	EAZ613	60.70	EAZ614	60.80	EAZ615	60.90	EAZ616	61.00	EAZ617	61.10	EAZ618	61.20	EAZ619	61.30	EAZ620	61.40	EAZ621	61.50	EAZ622	61.60	EAZ623	61.70	EAZ624	61.80	EAZ625	61.90	EAZ626	6
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CATALOGUE NO. 5870

The Jackson Friction Ball Drive Reduction Unit is unique. Simply because it's the only one of its type and size available in the United Kingdom. It has sealed lubrication, with a hardened steel shaft and bearings to give it extra long life. And it's low in price. The unit has a 10:1 reduction ratio, with an output torque of 8 oz. ins. minimum.

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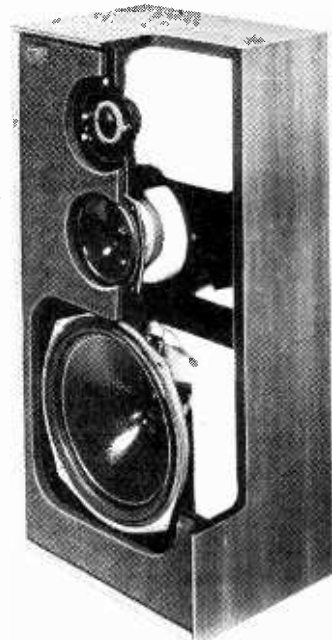
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WW-14 FOR FURTHER DETAILS

# Celestion Dittons for the perfectionist



**DITTON 44 MONITOR** 30x14½x10in (76x37x25cm) 44w  
Cut-away illustration showing the Celestion transducers – seen at the top HF 2000 Tweeter, now accepted as the world's finest; at centre, a FC6 mid-range using special rubber suspension, 50,000 Maxwell magnet, and transmission line rear loading; at the base, a FC12, this rugged long coil low resonance unit being tuned to its 43.47 litre hermetically sealed enclosure. On test has accepted quite safely transient signals ten times greater than the rated maximum wattage. Now recognised as providing an exceptional standard of sound reproduction by independent reviewers in England, the USA and Europe. A thoroughbred monitor class loudspeaker for the discerning listener, priced absolutely realistically.



**HADLEIGH** 13¾x10x9½in 20w  
(34x25x24cm)

The Hadleigh loudspeaker, was specially created to meet a public demand for a high quality speaker of compact proportions. Not a difficult task for Celestion who produce the most popular bookshelf speaker ever (Ditton 15) – but we set out not only to produce an immaculate loudspeaker with a sparkling performance, but to do so at a budget price. For the enthusiast seeking a really excellent Hi-Fi system at reasonable outlay we recommend without hesitation the Hadleigh.

## Celestion



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WW-093 FOR FURTHER DETAILS.

# QUALITY AMPLIFIER KITS by POWERTRAN ELECTRONICS

## WIRELESS WORLD AMPLIFIER DESIGNS

Component packs for a choice of three outstanding amplifiers are stocked together with packs for a regulated power supply suitable for use with a pair of any of them. Also stocked are packs for a very well-established pre-amplifier—the Bailey-Burrows design which features six inputs, a scratch and rumble filter and wide range tone controls which may be either rotary or slider operating.

### 30W BAILEY

- Pk. 1 F/Glass PCB £0.80
- Pk. 2 Resistors, capacitors, pots £1.75
- Pk. 3 Semiconductor set £4.70

### 20W LINSLEY-HOOD

- Pk. 1 F/Glass PCB £0.85
- Pk. 2 Resistors, capacitors, pots £2.40
- Pk. 3 Semiconductor set £3.35

### 60V REGULATED POWER SUPPLY

- Pk. 1 F/Glass PCB £0.75
- Pk. 2 Resistors, capacitors, pots £1.40
- Pk. 3 Semiconductor set £3.10

### BAILEY-BURROWS PRE-AMP

- Pk. 1 F/Glass PCB £2.05
- Pk. 2 Resistors, capacitors, pre-sets, transistors £4.95

- Pk. 3R Rotary potentiometer set £1.60
- Pk. 3S Slider potentiometer set (with knobs) £2.70

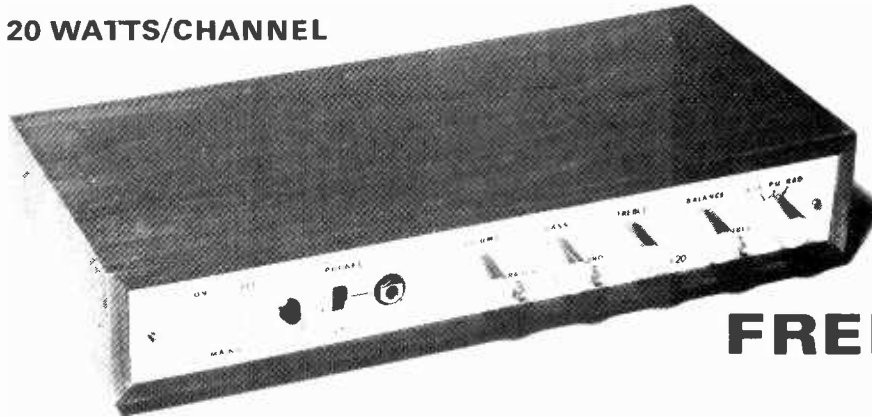
### STUART TAPE RECORDER

A set of three printed-circuit boards has been prepared for the stereo integrated circuit version of this high-performance *Wireless World* published design.

- TRRP Pk. 1 Reply amplifier F/Glass PCB £0.90
- TRRC Pk. 1 Record amp./meter drive cct. F/Glass PCB £1.40
- TROS Pk. 1 Bias/erase/stabilizer cct. F/Glass PCB £1.00

For details of component packs for this design please write for free list.

## 20 WATTS/CHANNEL



**FREE** TEAK CASE and HANDBOOK with full kits

KIT PRICE STILL ONLY **£28.25** post free (U.K.)

Pack	Price
1	Set of all low noise resistors £0.95
2	Set of all small capacitors £1.50
3	Set of 4 power supply capacitors £1.40
4	Set of miscellaneous parts including DIN sockets, fuses fuse holders, control knobs, etc. £1.90
5	Set of slide and push-button switches £1.20
6	Set of potentiometers and selector switch £2.00
7	Set of all semiconductors £7.25
8	Special Toroidal Transformer £4.95
9	Fibreglass PC Panel £2.50
10	Complete chassis work, hardware and brackets £4.20
11	Preformed cable/leads £0.40
12	Handbook £0.25
13	Teak Cabinet £2.75

### SEMICONDUCTORS AS USED IN OUR RANGE OF QUALITY AMPLIFIERS

2N699 £0.25	2N5459 £0.45	BC184L £0.11	MC1351 £1.05	SN72741P £0.40
2N1613 £0.20	2N5461 £0.50	BC212L £0.12	MFC4010 £0.95	SN72748P £0.40
2N1711 £0.25	2N5830 £0.30	BC214L £0.14	MJ481 £1.20	TIL209 £0.30
2N2926G £0.10	40361 £0.40	BCY72 £0.13	MJ491 £1.30	TIP29A £0.50
2N3055 £0.45	40362 £0.45	BD529 £0.85	MJE521 £0.60	TIP30A £0.60
2N3442 £1.20	BC107 £0.10	BD530 £0.85	MPSA05 £0.25	TIP29C £0.71
2N3704 £0.10	BC108 £0.10	BDY56 £1.60	MPSA12 £0.55	TIP30C £0.78
2N3707 £0.10	BC109 £0.10	BF257 £0.40	MPSA14 £0.35	TIP41A £0.74
2N3711 £0.09	BC109C £0.12	BF259 £0.47	MPSA55 £0.25	TIP42A £0.90
2N3904 £0.17	BC125 £0.15	BFR39 £0.25	MPSA65 £0.35	1N914 £0.07
2N3906 £0.20	BC126 £0.15	BFR79 £0.25	MPSA66 £0.40	1N916 £0.07
2N4062 £0.11	BC182 £0.10	BFV51 £0.20	MPSU05 £0.60	1S920 £0.10
2N4302 £0.60	BC212 £0.12	BFV52 £0.20	MPSU55 £0.70	5805 £1.20
2N5087 £0.42	BC182K £0.10	CA3046 £0.70	SBA750A £2.50	<b>FILTERS</b>
2N5210 £0.54	BC212K £0.12	LP1186 £5.50	SL301 £1.30	FM4 £0.80
2N5457 £0.45	RC182L £0.10	MC1310 £2.90	SL3045 £1.60	SFG10.7MA £2.80

### ACTIVE FILTER CROSSOVER

An essential and critical component in a high-quality speaker system is the crossover unit conventionally comprising of a series of passive networks which unfortunately, though introducing reactive impedances between the amplifier and the speakers, result in the loss of the advantage of high amplifier damping factor and renders the speakers prone to overshoots and resonances. An elegant solution to this problem, described by D. C. Read in *Wireless World*, involves the use of a series of active filters splitting the output of the pre-amplifier into three channels, of closely defined bandwidth, each of which is fed to the appropriate speaker by its own power amplifier. A design for a suitable 20-watt amplifier, based on a proven Texas circuit, was also described by Mr Read. The printed-circuit board for this has been designed such that three amplifiers may be stacked and mounted together on a common heat sink to achieve a conveniently compact module.

#### ACTIVE FILTER

- Pack 1 Fibreglass PCB (accommodates all filters for one channel) £1.05
  - 2 Set of pre-sets, solid tantalum capacitors, 2% metal oxide resistors, 2% polystyrene capacitors £4.20
  - 3 Set of semiconductors £2.65
- 2 off each pack required for stereo system

#### READ/TEXAS 20w amp.

- Pack 1 Fibreglass PCB £0.70
  - 2 Set of resistors, capacitors pre-sets (not including O/P coupling capacitors) £1.10
  - 3 Sets of semiconductors £2.40
  - 6 off each pack required for stereo system
  - 4 Special heat sink assembly for set of 3 amplifiers £0.85
  - 5 Set of 3 O/P coupling capacitors £1.00
- 2 off packs 4, 5 required for stereo system

#### POWER SUPPLY

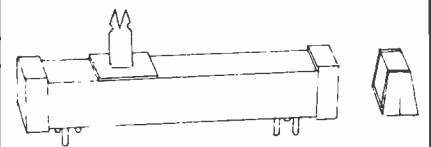
- FOR 20W/CHANNEL STEREO SYSTEM
- Pack 1 Fibreglass PCB £0.50
- 2 Set of rectifiers, zener diode, capacitors, fuses, fuse holders £2.60
- 3 Toroidal transformer £4.95

SUITABLE ALSO FOR FEEDING ANY OF OUR HIGH-POWER DESIGNS

**MORE KITS ON PAGE 47!**

for further information please write for **FREE LIST NOW!**

## ★ SPECIAL OFFER ★



### SLIDER POTENTIOMETER SALE!

Most values 1K-1M lin/log available

	Normal price	Sale Price
Single	35p	25p
Dual	55p	35p
Knob	15p	10p

V.A.T. Please add 25%\* to all U.K. orders

(\*or at current rate if changed)

U.K. ORDERS—Post free (mail order only)

SECURICOR DELIVERY—for this optional service (Mainland only) add £2.00 + VAT per kit

OVERSEAS—Postage at cost + 50p special packing, handling

Dept. WW06

**POWERTRAN ELECTRONICS**

PORTWAY INDUSTRIAL ESTATE ANDOVER, HANTS SP10 3NN

# BI-PRE-PAK

**Bargains in Semi-Conductors, components, modules & equipment.**

## Bargains from our FREE Catalogue

20 large pages, filled with real bargains in transistors, I.C.s, components, equipment, etc. Send large S.A.E. with 7p stamp for your FREE copy of 6th Edition by return. Meanwhile, for prompt delivery why not order from this month's ad. NOW. Payment may be made by Access.

### TRANSISTOR PACKS ALL AT 50p EACH TESTED & GUARANTEED

<b>B79</b>	<b>4</b>	IN4007 Sil. Rec. diodes 1.000PIV 1 amp plastic	<b>H39</b>	<b>6</b>	Integrated circuits 4 gates BMC 962, 2 flip flops BMC945
<b>B81</b>	<b>10</b>	Reed Switches. 1" long 1/8" dia High-speed P.O. type	<b>H41</b>	<b>2</b>	BD131/BD132 Complementary Plastic Transistors 40361 Type NPN Sil Transistors TO-5 can comp. to H66
<b>H35</b>	<b>100</b>	Mixed Diodes. Germ. Gold bonded, etc. Marked and Unmarked.	<b>H65</b>	<b>4</b>	40362 Type PNP Sil Transistors TO-5 can comp. to H65
<b>H38</b>	<b>30</b>	Short lead. NPN Silicon Planar Ex Equipment.			

### UNMARKED & UNTESTED PACKS—50p EACH

<b>B1</b>	<b>50</b>	Germanium Transistors PNP, AF and RF	<b>B86</b>	<b>100</b>	Sil Diodes sub min. IN914 and IN916 types
<b>B66</b>	<b>150</b>	Germanium Diodes Min. Glass type	<b>H34</b>	<b>15</b>	Power Transistors PNP Germ. NPN Silicon TO-3 Can
<b>B84</b>	<b>100</b>	Silicon Diodes DO-7 Min glass equivalent to IN4148	<b>H67</b>	<b>10</b>	3B19N Channel FET's plastic case type

### PLASTIC POWER TRANSISTORS

40 WATT SILICON				
Type	Polarity	Gain	VCE	Price
40N1	NPN	15	15	20p
40N2	NPN	40	40	30p
40P1	PNP	15	15	20p
40P2	PNP	40	40	30p

90 WATT SILICON				
Type	Polarity	Gain	VCE	Price
90N1	NPN	15	15	25p
90N2	NPN	40	40	35p
90P1	PNP	15	15	25p
90P2	PNP	40	40	35p

**LM 380 AUDIO IC** (Marked 60745). Brand new and to spec. 3 watts R.M.S. out. With data **£1**

**PAK No. 1.** Short lead semiconductor and components on PCBs marked. Up to 170 Herz Date. **50p**

**TWO GOOD IC OFFERS.** Brand new, to spec. Two SN 7490 decade counters. **£1**

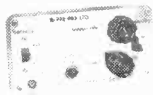
**THREE SN 7400 Quad 2 input Nan gate ICs** **50p**

### CAPACITOR DISCHARGE IGNITION KIT

Simple to assemble and fit. Improves car performance. saves on fuel. P/P 30p

**£7.50**

### Bi-Pre-Pak X-Hatch Generator Mk. 2



- Four-pattern selector switch 3"x5 1/4"x3"
- Ready-built and tested **£9.93\***
- In kit form **£7.93\***

Please add 30p for postage and packing

Is invaluable to industrial and home user alike. Improved circuitry assures reliability and still better accuracy. Very compact; self-contained. Robustly built. Widely used by TV rental and other engineers. With reinforced fibreglass case, instructions, but less batteries. (Three U2 type required.)

### TV SIGNAL STRENGTH METER

Complete kit as described in "Television" **£19.50** plus 40p for P&P

#### MAINS TRANSFORMERS

A. 18V 1 amp (suitable for SS 103)	<b>£1.50</b>
B. 25V 2 amp (suitable for SS 110)	<b>£2.00</b>
C. 30V 2 amp (suitable for SS 140)	<b>£4.50</b>

Add 35p for P&P per transformer

#### BRIDGE RECTIFIERS

Type A 45V/1A 27p B & C 100V/2A **36p**

**MAINS RELAYS** 230, 240V AC 3-pole change-over heavy duty contacts **60p**  
Ex-GPO Telephone Handsets, each **55p**

**TO CLEAR.** Hundreds of various portable transistor radio chassis with FM & AM tuning. Ideal for experimenters. All components in good electronic order, but no instructions or tuning drives per chassis. Each **£1.00**. 8 assorted relays **£1.00**. Rev. counter device (for cars) **£1.00**. U.H.F./TV Tuner Units 625 line, rotary control **£2.50**. Technical books of all kinds including Newnes & Butterworth, Bernards Press, etc.

## BI-PRE-PAK LTD

Co Reg No 820919

222 224 WEST ROAD, WESTCLIFF-ON-SEA, ESSEX SSO 9DF.

TELEPHONE: SOUTHEND (0702) 46344.

Made and sold direct by Bi-Pre-Pak



## Stirling Sound

Today's most challenging values!

### AMPLIFIER MODULES

<b>SS100</b>	Active tone control unit to provide Bass and Treble facilities (stereo).	<b>£1.60</b>
<b>SS101</b>	Pre-amp for stereo ceramic cartridges, radio and tape.	<b>£1.60</b>
<b>SS102</b>	Pre-amp for low-output stereo magnetic cartridges, radio and tape.	<b>£2.25</b>
<b>SS103</b>	Compact I.C. amp. 3 watts R.M.S. Single channel (mono). On P.C.B. size 3 1/2"x2". Needs 10-20V supply	<b>£1.75</b>
<b>SS103-3</b>	Stereo version of above. (Two I.C.s.)	<b>£3.25</b>
<b>SS105 Mk. 2</b>	Improved design and performance. A compact all-purpose power amp. Can be run from 12V car battery. Size 3 1/2" x 2". Useful 5w output (mono). Excellent value	<b>£2.25</b>
<b>SS110 Mk. 2</b>	Similar in size to SS105 Mk. 2 but will give 10w output (mono). Two in stereo give first-class results, suitable for many domestic applications.	<b>£2.75</b>
<b>SS140</b>	Beautifully designed. Will give up to 40w R.M.S. into 4Ω. Excellent S.N.R. and transient response. Fine for P.A., disco use, etc. Operates from 45V DC. Two in bridge formation will give 80w R.M.S. into 8Ω.	<b>£3.60</b>
<b>FM TUNER MODULES</b>		
<b>SS201</b>	Front End assembly. Ganged tuning with well engineered slow-motion geared drive in robust housing. A.F.C. facility. Requires 6-16V. Excellent sensitivity. Tuners from 88-108MHz	<b>£6.25</b>
<b>SS202</b>	I.F. Stage (with I.C.) Designed to use with SS201. Uses I.C. Carefully checked before despatch.	<b>£5.25</b>
<b>SS203</b>	Stereo Decoder. Designed essentially for use with SS201 and SS202, this excellent decoder can also make a stereo tuner of almost any single channel FM tuner. Supplied ready aligned. A LED can easily be fitted for stereo reception indication.	<b>£5.62</b>
<b>SS300</b>	<b>POWER SUPPLY STABILISER.</b> Add this to your unstabilised supply to obtain a steady working voltage from 16 to 60V for your audio system, workbench, etc. Money saving and very reliable	<b>£5.62</b>

### SPECIAL F.M. TUNER OFFER TO SAVE YOU £5

Buy Stirling Sound Units SS201, 202 and 203 together to make a first class stereo F.M. tuner, total advertised price £17.12 and it will cost you only giving a genuine saving of £5.

**£12.12**

### BI-PRE-PAK COMPONENT PACKS — ALL 50p EACH

<b>CP1</b>	<b>150</b>	Capacitors, mixed (Electrolytic Silver Mic. Quantity approx. sold by weight)	<b>CP4</b>	<b>12</b>	Pots, pre-sets, mixed W/wound carbons, dual with/without switches
<b>CP2</b>	<b>200</b>	Resistors, mixed values and wattage (Quantity approx. sold by weight)	<b>CP7</b>	<b>25</b>	Heat sinks assorted To fit SO2 (OC72) TO-1 (AC 128) etc
<b>CP3</b>	<b>40</b>	Wirewound resistors Mixed types and values	<b>CP10</b>	<b>3</b>	2.5mm plugs sub-miniature White bodies
			<b>CP11</b>	<b>6</b>	Screwdrivers 1 x mains neon tester. 5 grub types (8%)

**TERMS OF BUSINESS:** VAT at 25% must be added to total value of order including postage and packing charges. For prices marked \* or (8%) please add 8% for VAT. No VAT on overseas orders. **POST & PACKING** Add 20p for UK orders. Minimum mail order acceptable — £1. Overseas orders, add £1 for postage. Any difference will be credited or charged. **PRICES** Subject to alteration without notice. **AVAILABILITY** All items available at time of going to press when every effort is made to ensure correctness of information.

### To BI-PRE-PAK, 222-224 WEST ROAD WESTCLIFF-ON-SEA, ESSEX

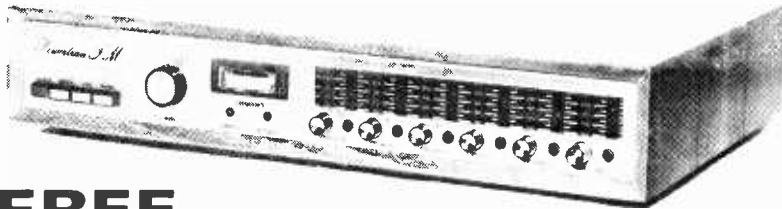
Please send .....  
for which I enclose ..... inc. VAT  
NAME .....  
ADDRESS .....  
..... WW7

Pack	Price	Pack	Price
1 Fibreglass printed circuit board for front end, I.F. strip, demodulator, AFC and mute circuits	£2.15	9 Function switch, 10 turn tuning potentiometer, knobs	£5.30
2 Set of metal oxide resistors, thermistor, capacitors, cermet preset for mounting on pack 1	£4.80	10 Frequency meter, meter drive components, fibreglass printed circuit board	£8.60
3 Set of transistors, diodes, LED, integrated circuits for mounting on pack 1	£6.25	11 Toroidal transformer with electrostatic screen, Primary: 0-117V-234V	£4.45
4 Pre-aligned front end module, coil assembly, three-section ceramic filter	£8.80	12 Set of capacitors, rectifiers, voltage regulator for power supply	£2.95
5 Fibreglass printed circuit board for stereo decoder	£1.10	13 Set of miscellaneous parts, including sockets, fuse holder, fuses, inter-connecting wire, etc.	£1.50
6 Set of metal oxide resistors, capacitors, cermet preset for decoder	£2.60	14 Set of metal work parts including silk screen printed fascia panel, acrylic silk screen printed tuning indicator panel insert, internal screen, fixing parts, etc.	£6.50
7 Set of transistors LED integrated circuit for decoder	£3.45	16 Teak cabinet	£7.35
8 Set of components for channel selector switch module including fibreglass printed circuit board, push-button switches, knobs, LEDs preset adjusters, etc.	£8.30	One each of packs 1-16 inclusive are required for complete stereo FM tuner	£74.10
		Total cost of individually purchased packs	£74.10

**NOVEL STEREO FM TUNER**

In the April and May 1974 issues of *Wireless World* there was published by J. Skingley and N. C. Thompson a novel design for an f.m. tuner which combines consistent high performance with the elimination of the critical setting-up procedure required by too many earlier tuners. The front end is a ready built pre-aligned module which then feeds an amplifier driven screened three section ceramic filter leading to an integrated circuit five-stage limiting amplifier providing excellent a.m. rejection. This is followed by a single coil integrated balanced demodulator from which the audio output may be taken. Temperature compensated varicap tuning allows stations to be selected either by a ten-turn tuning potentiometer or by a choice of six preset push-button controls. Each of the preset controls can be adjusted on the front panel with the settings being indicated by six LED lamps behind an acrylic silk screen printed fascia panel insert. Additional circuitry includes temperature compensated AFC restricted to less than station spacing, inter-station muting, a single-lamp LED tuning indicator and a linear scale frequency meter. The stereo decoder, built on a separate board, is based on a well-proven integrated circuit phase-locked-loop to which has been added active filters to remove sub carrier harmonics and 'birdies'. The power supply, to ensure station holding stability, uses an integrated circuit voltage regulator which is powered via a low-hum field specially designed TOROIDAL TRANSFORMER.

**STYLED TO COMPLEMENT THE WORLD-WIDE ACCLAIMED LINSLEY-HOOD 75W AMPLIFIER**



**FREE TEAK CASE WITH FULL KITS**

KIT PRICE only **£66.75** carriage free (U.K.)

**THE FM TUNER KIT YOU HAVE WAITED FOR!**

for further information please write for **FREE LIST**

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**NEW!**

FROM

**POWERTRAN ELECTRONICS**

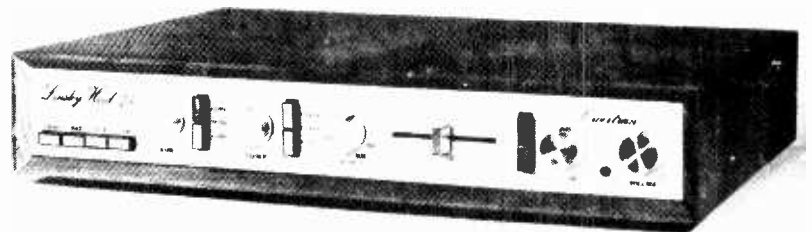
MORE ON NEXT PAGE!

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**DESIGNER APPROVED KIT**

In *Hi-Fi News* there was published by Mr Linsley-Hood a series of four articles (November 1972-February 1973) and a subsequent follow-up article (April 1974) on a design for an amplifier of exceptional performance which has as its principal feature an ability to supply from a direct coupled fully protected output stage, power in excess of 75 watts whilst maintaining distortion at less than 0.01% even at very low power levels. The power amplifier is complemented by a pre-amplifier based on a discrete component operational amplifier referred to as the Liniac which is employed in the two most critical points of the system, namely the equalization stage and tone control stage, positions where most conventional designs run out of gain at the extremes of the frequency spectrum. Unusual features of the design are the variable transition frequencies, of the tone controls and the variable slope of the scratch filter. There is a choice of four inputs, two equalized and two linear, each having independently adjustable signal level. The attractive slimline unit pictured has been made practical by highly compact PCBs and a specially designed Toroidal transformer.

Hi-Fi News Linsley-Hood 75W/Channel Amplifier Mk III Version (modifications as per *Hi-Fi News* April 1974)



Full circuit description in handbook (pack 15—price 30p)

**FREE** TEAK CASE WITH FULL KITS  
KIT PRICE only **£62.40** carriage free (U.K.)

V A T Please add 25%\* to all U.K. orders -

(\* or at current rate if changed)

U K ORDERS—Post free (mail order only)

SECURICOR DELIVERY: For Securicor delivery to mainland—add £2 + VAT per kit.

OVERSEAS—Postage at cost + 50p special packing

Dept. WW06

**POWERTRAN ELECTRONICS**

PORTWAY INDUSTRIAL ESTATE

ANDOVER, HANTS SP10 3NN

Pack	Price	Pack	Price
1 Fibreglass printed circuit board for power amp	£0.85	11 Fibreglass printed-circuit board for power supply	£0.65
2 Set of resistors, capacitors, pre-sets for power amp.	£1.70	12 Set of resistors, capacitors, secondary fuses, semiconductor for power supply	£3.50
3 Set of semiconductors for power amp. (now using BDY56 BD529, BD530)	£6.50	13 Set of miscellaneous parts including DIN skts, mains input skt, fuse holder inter-connecting cable, control knobs	£4.25
4 Pair of 2 drilled, finned heat sinks	£0.80	14 Set of metalwork parts including silk screen printed fascia panel and all brackets, fixing parts etc.	£6.30
5 Fibreglass printed circuit board for pre-amp	£1.30	15 Handbook	£0.30
6 Set of low noise resistors, capacitors, pre-sets for pre-amp	£2.70	16 Teak cabinet	£7.35
7 Set of low noise, high gain semiconductors for pre-amp	£2.40	2 each of packs 1-7 inclusive are required for complete stereo system	£69.75
8 Set of potentiometers (including mains switch)	£2.05	Total cost of individually purchased packs	£69.75
9 Set of 4 push button switches, rotary mode switch	£3.70		
10 Toroidal transformer complete with magnetic screen/housing primary 0 117-234 V, secondaries: 33-0-33 V 25-0-25 V.	£9.15		

WW-074 FOR FURTHER DETAILS

### MAINS TRANSFORMERS

All standard to 230-250 volt primaries

1v	1 amp (special)	£ 1.75
2.4v	5 amp	85
6.3v	2 amp	1.00
6.3v	3 amp	1.50
9v	1 amp	.95
9v	3.5 amp	1.95
12v	2 amp	1.50
12v	1 amp	1.00
15v-0-6.5v	1 amp	1.35
18v	1 amp	1.25
20v	3 amp	1.50
20v	1 amp	1.50
24v	3 amp	3.50
24-0-12v	50mA	1.20
24-0-12v	50mA	1.20
6-0-6v	4 amp	1.25
8-0-8v	2 amp	3.50
18-0-18v	3 amp	1.95
25v	1 amp	1.50
50v 2 amp & 6.3v	1 amp	5.50
60v 5 amp & 5v	8 amp	7.50
27v	37 amp	4.50
30v	4 amp	22.00
80v tapped 75v & 70v	4 amp	5.50
230v-60mA & 6.3v	1.5 amp	1.75
275-0-275v at 90mA & 6.4v	3 amp	2.25
EHT Transformer 5kV at 23mA (intermittent)	1 amp	5.50

#### Charger Transformers

6v and 12v	2 amp	1.25
6v and 12v	3 amp	2.25
6v and 12v	5 amp	3.50

### HONEYWELL PROGRAMMER

This is a drum type timing device... Price from makers probably over £20 each. Special snip price **£8.50** plus 25p post and insurance. Don't miss this terrific bargain.

### SWITCH TRIGGER MATS

So thin is undetectable under carpet but will switch on with slightest pressure. For burglar alarms, shop doors, etc.

### MULLARD UNILEX STEREO SYSTEM

There is no doubt that it is a good system, we believe that for the money it is without comparison.

1 Unilex Amplifier	Ref. EP 9000	£1.75
1 Unilex Amplifier	Ref. EP 9000	£1.75
1 Unilex Pre-Amp	Ref. EP 9001	£2.00
1 Unilex Power Unit	Ref. EP 9002	£2.50

1 Control panel kit with spun aluminium-faced knobs **£3.80**

Pair of 15 ohm speakers made by Goodmans are also available if required, price **£3.30** the pair. No extra postage if ordered with the above, otherwise add 25p.

### INFRA RED BINOCULARS

Made for military purposes during and immediately after last war to enable snipers, vehicle drivers etc. to see in the dark... Price **£16.50** per set + £1 carriage.

### NEW ITEMS THIS MONTH

AC mains operated relay with single changeover 10 amp contacts open type single screw fixing through the base 50p each.

Battery condition testers. This is another item which has been out of stock temporarily but we are pleased to say, in stock again. Price now **£3.50**.

AM/FM tuning condenser as fitted to many Japanese and Hong Kong portables, has two main tuning sections and four trimmers. Approx size 1" x 1" x 1" 60p each.

Battery charger kit comprising 2 amp transformer, 2 amp full wave rectifier and 2 amp meter suitable for charging 6v or 12v. Special bargain price **£1.50** the kit + 30p post.

MacDonald record auto-changer with tuning arm and ceramic stereo cartridge. This is a very superior auto-changer and one we can thoroughly recommend. Limited quantity, special price **£7.35** + £1 post and insurance. Plinth and cover (the plinth has to be modified very slightly) available, price **£4.95** + £1 post or if you buy both together you can get a discount of £1.

Instrument case measures 18" x 12" x 12". This is a very well-made case built on an angled framework, has rounded corners and edges into this framework fit the 8 panels. All panels are hinged for ventilation, side panels are also fitted with handles, the bottom panel has 4 rubber feet. These instrument cases, would probably cost around **£15** each. We have approx 100, not new but in very good condition and offer them at **£3** each.

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3 core lead, 7' 6" long, ribbed, virtually non-kinkable 23/36 conductors, so OK for 8 amps. Price 10p each.

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Cold cathode tube Swiss made "Elasta" type No ER 12A. We have no technical information on this tube and if any reader has this we will be obliged for any information. Price of the tubes 30p each.

Push switch, double pole changeover contacts rated at 10 amps 250 volts made by the American Honeywell Co. A very reliable and robust switch with plenty of applications. Oblong plastic body, snap fitting into a hole size 1 1/2" x 1". Offered at only a fraction of its proper price, namely **20p** each.

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2	Twice Daily	Off
3	All Day	Off
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5	All Day	All Day
6	Continuously	Continuously

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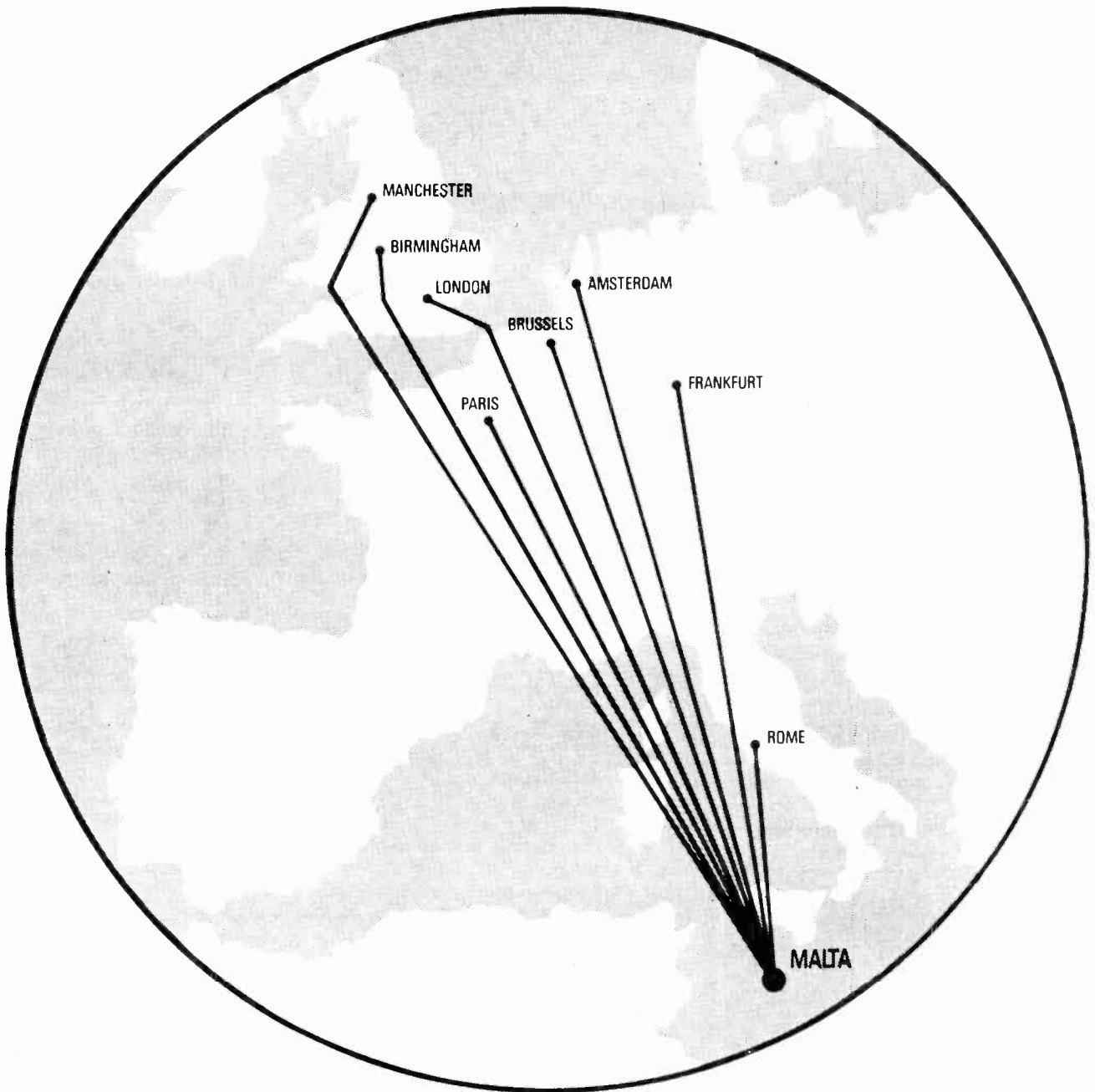
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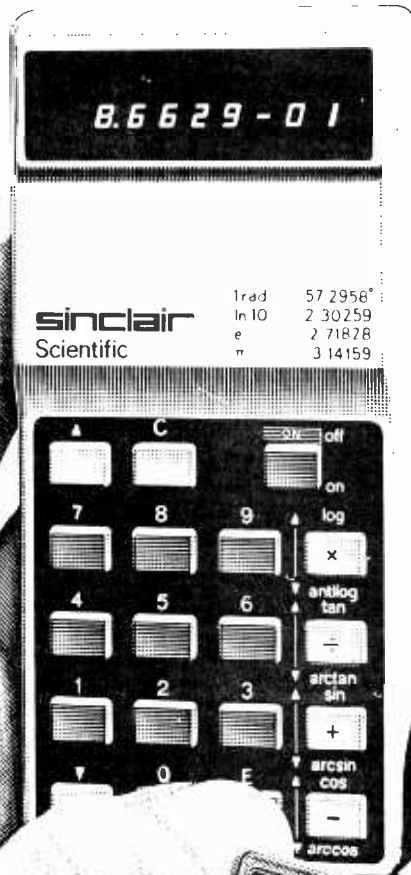
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\* TERNAL TRIGGERING. 230-250v. A.C. OPERATION. \*  
\* RANGE OF 4 STROBE KITS FROM STOCK. \*  
\* PRICES FROM £6.30-£22.00. SAE FOR \*  
\* DETAILS \*  
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\* 400 Watt Mercury vapour ultra violet lamp \*  
\* Extremely compact and powerful source of u.v. \*  
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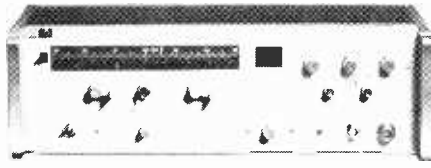
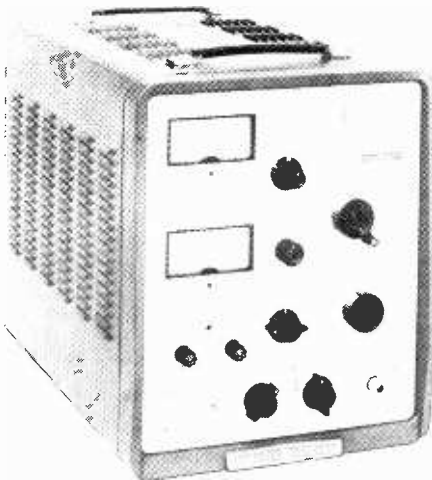
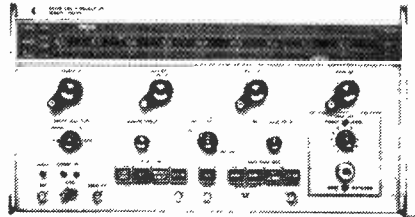
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<b>BRIDGES, ETC.</b> <b>Wayne Kerr</b> 601Z. LCR Bridge. Wide Frequency range	£80	546. DC-50MHz. Main Frame with delayed sweep dual time base	£240-£350	<b>SWEET GENERATORS</b> <b>Hewlett Packard</b> 8693B. 3.7-7.8GHz plug-ins (For use with 8690 Main Frame)	£290-£498
SR26B. Source & Detector	£109	547. DC-50MHz. Main Frame with delayed sweep dual time base	£280-£390	<b>TELEPHONE TV AND MICROWAVE</b> <b>Hewlett Packard</b> 3701/02/03. Microwave Link Analyser	£2,420
B221/Q221. LCR Bridge	£159	1A1. Plug-in for 546 or 547 DC-50MHz 5mV-20V/Div. Dual Trace	£90-£290	<b>Marconi</b> OA 2090A. White Noise Test Set	£712
B224. LCR Bridge	£179	1A2. Plug-in for 546 or 547. DC-50MHz. 50mV-20V/Div Dual Trace	£70-£120	(Filters also available at extra charge)	
<b>COUNTERS &amp; TIMERS</b> <b>Hewlett Packard</b> 3734. 5 Digits 3 Hz-5MHz	£50	585. DC-80MHz. Main Frame with Delay Time Base	£240-£400	TF 2905/5. Sin 2 P & B. Gen. 525 lines 60Hz	£298
5221A. 6 Digits. 5 Hz-10MHz	£80	82. Plug-in for 585. DC-80MHz. 100mV-50V/Div. Dual Trace	£50-£90	TF 2909. Grey Scale Gen. 625 lines	£440-£750
5216. 7 Digits. 12MHz	£198	564. DC-10MHz/14GHz. Storage or Sampling Main Frame	£220-£350	<b>Philips</b> PM 5508B. Pattern Gen. 625 lines PAL	UK Systems £159-£280
5245. 8 Digits. DC-50MHz. 3 x 10 <sup>-1</sup> per day ageing rate	£90-£550	Necessary plug-ins supplied (Real time and Sampling)	£40-£400		
5246. 6 Digit Counters DC-50MHz	£198	<b>Solartron</b> CD1740. DC-50MHz. Main Frame			
5252A. Pre-Scaler plug-ins. 350MHz	£90-£115	CX1741. Plug-in. DC-50MHz 5mV-20V/cm Dual Trace			
5253B. Converter plug-ins. 512MHz	£46-£182	CX1744. Plug-in. Time Base 0.5µs-1s/cm (Complete)	£295-£390		
5254C. Converter plug-ins. 0.15-3GHz	£159-£300	<b>Tequipment</b> D53S with 2 x 'A' amps. Storage. Dual Trace	£220		
5255A. Converter plug-ins. 3-12.4GHz	£280-£490	A. DC-15MHz. Single Trace Amplifier plug-ins (Two Plug-ins per Main Frame)	£10-£20		
5260A. Automatic Divider Unit. DC-12.4GHz (use with 50MHz Counter)	£570-£980				
<b>Marconi</b> TF1417/A. 6 Digits 0-15MHz	£130				
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TF2502. Power Meter	£130				
TF934. Power Meter	£80-£120				
<b>DIGITAL VOLTMETERS</b> <b>Dana</b> 3800A. Digital Multimeter 0.1% Max RDG 1999	£98-£140				
5230. DVM. 0.02% 10µV Max RDG 119999	£349-£450				
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<b>Dynacore</b> DM2022. D40 DC. 0.02% 10µV resolution-2kV	£98-£340				
DM2140/A1/B1. Mean AC Converters	£98-£240				
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Complete with 3482 DC plug-in					
3484 Multimeter Plug-in	£349				
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LM1420BA. DC and RMS/Mean A C	£319-£400				
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LM1480.3. Max. Rdg. 29999 5µV-2kV DC. Auto-ranging	£280				
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LM1867. Max. Rdg. 101999. 10µV-1kV DC	£259				
*Requires heads and recalibration.					
<b>POWER SUPPLIES</b> <b>Farnell</b> 30/10. 0-30V 10A Pre-set	£38-£50				
SSE. 0-15V 1A Pre-set	£22-£40				
<b>RECORDERS</b> <b>Bell &amp; Howell</b> 5-127 Ultra Violet Light Beam 12 Channels	£269				
(Galvos to 13kHz available at extra charge)					
<b>SIGNAL SOURCES</b> <b>General Radio</b> 1363. UHF Oscillator (needs power supply)	£80				
<b>Muirhead</b> D880A. 0.01Hz-11.2kHz. Decade. 2 Phase	£120-£198				
D890 1Hz-111.1kHz Decade 0-7V	£230				
<b>Marconi</b> TF144H/4 10kHz-72MHz. Xtal. check Int/Ext AM 50 ohms	£198-£320				
TF801D/1 10MHz-470MHz Int/Ext AM and Pulse modulation	£259				
<b>Wayne Kerr</b> O.22D. 10KHz-10MHz Video Oscillator	£98				
<b>Richmond Hill</b> TSP. TV Studio Precision Signal Generator Sin 2 P & B. Window. Starcase 525 lines. Requires all drives (Modification to 625 lines arranged at extra charge)	£290				
<b>Siemens</b> REL3K53. Contact Fault Locators. 1MHz Test Signal Variable levels. High sensitivity	£80				
<b>STC</b> 74166. Milliwatt Test Sets	£36-£45				
74184B. Selective Measuring Sets	£80				
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74306B. Oscillators 10kHz-20MHz	£80-£110				
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VZMG1. Sampling Attachments (Complete)	£310				
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<b>WAVE ANALYSERS</b> <b>Airmec/Racal</b> 248A. 5-300MHz. Harmonic Analysers	£132				
<b>ASSOCIATED EQUIPMENT</b> <b>Marconi</b> TF2606. Differential Voltmeter. 0-1000V	£120				
<b>Radiometer</b> RV24. D.C. Electronic Multimeter	£20*				
<b>Siemens</b> Multizet. R.F. Voltmeter. 0-100V	£5*				
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	1	25	100+
SN7400	0.14	0.13	0.12
SN7401	0.14	0.13	0.12
SN7402	0.14	0.13	0.12
SN7403	0.14	0.13	0.12
SN7404	0.15	0.14	0.13
SN7405	0.15	0.14	0.13
SN7406	0.30	0.29	0.28
SN7407	0.30	0.29	0.28
SN7408	0.15	0.13	0.12
SN7409	0.15	0.13	0.12
SN7410	0.14	0.13	0.12
SN7411	0.23	0.22	0.21
SN7412	0.19	0.18	0.17
SN7413	0.30	0.29	0.28
SN7414	0.71	0.70	0.69
SN7415	0.30	0.29	0.27
SN7416	0.28	0.27	0.26
SN7417	0.28	0.27	0.26
SN7420	0.14	0.13	0.12
SN7421	0.95	0.94	0.93
SN7422	0.25	0.24	0.23
SN7423	0.26	0.25	0.22
SN7425	0.26	0.25	0.22
SN7426	0.26	0.25	0.22
SN7427	0.26	0.25	0.22
SN7428	0.39	0.38	0.37
SN7430	0.14	0.13	0.12
SN7432	0.25	0.24	0.22
SN7433	0.36	0.35	0.34
SN7437	0.27	0.26	0.22
SN7438	0.27	0.26	0.22
SN7439	1.10	1.08	1.06
SN7440	0.14	0.13	0.12
SN7441	0.70	0.69	0.66
SN7442	0.63	0.60	0.53
SN7443	1.00	0.99	0.90
SN7444	1.08	1.07	1.05
SN7445	0.85	0.83	0.70
SN7446	1.03	1.00	0.85
SN7447	1.03	1.00	0.85
SN7448	0.85	0.83	0.70
SN7450	0.14	0.13	0.12
SN7451	0.14	0.13	0.12
SN7453	0.14	0.13	0.12
SN7454	0.14	0.13	0.12
SN7455	0.40	0.39	0.38
SN7460	0.14	0.13	0.12
SN7462	0.45	0.44	0.42
SN7464	0.45	0.44	0.42
SN7465	0.45	0.44	0.42
SN7470	0.30	0.27	0.25
SN7471	0.60	0.59	0.58
SN7472	0.25	0.24	0.21
SN7473	0.30	0.27	0.26
SN7474	0.31	0.29	0.26
SN7475	0.40	0.39	0.38
SN7476	0.31	0.29	0.26
SN7478	0.65	0.63	0.61
SN7480	0.43	0.41	0.36
SN7481	1.00	0.95	0.90
SN7482	0.75	0.70	0.62
SN7483	0.81	0.80	0.68
SN7484	0.90	0.86	0.85
SN7485	1.25	1.15	1.00
SN7486	0.31	0.28	0.25
SN7489	3.50	3.20	3.00
SN7490	0.45	0.42	0.35
SN7491	1.00	0.95	0.90
SN7492	0.45	0.42	0.35
SN7493	0.45	0.42	0.35
SN7494	0.48	0.45	0.40

	1	25	100+
SN7495	0.60	0.56	0.50
SN7496	0.70	0.67	0.60
SN7497	0.70	0.69	0.68
SN74100	1.35	1.30	1.25
SN74104	0.31	0.29	0.26
SN74105	0.31	0.29	0.26
SN74107	0.31	0.29	0.26
SN74109	1.00	0.97	0.95
SN74110	0.55	0.50	0.45
SN74111	0.81	0.80	0.76
SN74114	1.00	0.97	0.95
SN74115	1.00	0.97	0.95
SN74118	1.00	0.95	0.90
SN74121	0.31	0.29	0.25
SN74122	0.44	0.41	0.37
SN74123	0.62	0.58	0.50
SN74125	0.70	0.65	0.60
SN74126	0.75	0.70	0.65
SN74128	1.40	1.35	1.30
SN74132	2.10	2.05	2.00
SN74136	0.95	0.90	0.85
SN74140	2.50	2.45	2.40
SN74141	0.75	0.70	0.62
SN74145	1.15	1.10	1.05
SN74147	2.95	2.90	2.85
SN74148	2.30	2.25	2.20
SN74150	1.35	1.30	1.25
SN74151	0.68	0.62	0.55
SN74152	1.55	1.50	1.45
SN74153	0.68	0.62	0.55
SN74154	1.55	1.50	1.45
SN74155	0.68	0.62	0.55
SN74156	0.68	0.62	0.55
SN74157	0.90	0.85	0.80
SN74158	1.50	1.45	1.40
SN74160	0.95	0.90	0.80
SN74161	0.95	0.90	0.80
SN74162	0.95	0.90	0.80
SN74163	0.95	0.90	0.80
SN74164	1.60	1.55	1.50
SN74165	1.60	1.55	1.50
SN74166	1.40	1.30	1.15
SN74170	2.40	2.30	2.20
SN74173	1.65	1.60	1.55
SN74174	1.15	1.10	1.00
SN74175	0.97	0.90	0.80
SN74176	1.10	1.05	1.00
SN74177	1.10	1.05	1.00
SN74180	1.10	1.05	1.00
SN74181	3.50	3.45	3.35
SN74182	1.10	1.05	1.00
SN74184	1.60	1.55	1.50
SN74185	2.30	2.25	2.20
SN74188	4.90	4.85	4.80
SN74190	1.75	1.70	1.65
SN74191	1.70	1.65	1.60
SN74192	1.25	1.05	1.00
SN74193	1.25	1.05	1.00
SN74194	1.10	1.05	1.00
SN74195	0.90	0.85	0.80
SN74196	1.05	1.00	0.95
SN74197	1.05	1.00	0.95
SN74198	2.05	2.00	1.70
SN74199	2.05	2.00	1.70
SN74200	6.00	5.95	5.80
SN74221	1.80	1.75	1.70
SN74251	1.80	1.75	1.70
SN74278	3.00	2.90	2.80
SN74279	1.20	1.15	1.10
SN74293	1.00	0.95	0.90
SN74298	2.60	2.55	2.50

### C-MOS Types

	1	25	100+
4000AE	0.24	0.19	0.16
4001AE	0.24	0.19	0.16
4002AE	0.24	0.19	0.16
4004AE	4.90	4.80	4.70
4006AE	1.55	1.50	1.45
4007AE	0.24	0.19	0.16
4008AE	1.60	1.55	1.50
4009AE	0.35	0.34	0.30
4010AE	0.50	0.48	0.46
4011AE	0.24	0.19	0.16
4012AE	0.24	0.19	0.16
4013AE	0.59	0.47	0.39
4014AE	1.65	1.33	1.10
4015AE	1.65	1.33	1.10
4016AE	0.62	0.50	0.41
4017AE	1.62	1.31	1.08
4018AE	2.45	2.40	2.30
4019AE	0.62	0.50	0.41
4020AE	1.82	1.46	1.21
4021AE	1.65	1.33	1.10
4022AE	1.65	1.33	1.10
4023AE	0.24	0.19	0.16
4024AE	1.13	0.91	0.75
4025AE	0.24	0.19	0.16
4026AE	6.50	6.40	6.30
4027AE	0.42	0.41	0.40
4028AE	1.41	1.14	0.94
4029AE	1.95	1.57	1.30
4030AE	0.62	0.50	0.41
4033AE	2.80	2.70	2.60
4035AE	1.71	1.38	1.14
4040AE	1.82	1.46	1.21
4041AE	0.90	0.85	0.80
4042AE	1.00	0.90	0.80
4043AE	1.00	0.90	0.80
4044AE	1.00	0.90	0.80
4047AE	1.50	1.45	1.40
4048AE	1.30	1.25	1.20
4049AE	0.54	0.44	0.36
4050AE	0.54	0.44	0.36
4051AE	1.77	1.43	1.18
4052AE	2.00	1.90	1.80
4053AE	2.70	2.60	2.50
4055AE	2.60	2.50	2.40
4056AE	1.35	1.09	0.90
4060AE	2.25	1.82	1.50
4066AE	0.95	0.90	0.85
4069AE	0.38	0.30	0.25
4071AE	0.34	0.27	0.23
4076AE	1.45	1.40	1.35
4081AE	0.34	0.27	0.23
4510AE	1.75	1.70	1.65
4516AE	1.76	1.42	1.18
4518AE	2.17	1.75	1.45
4520AE	1.65	1.60	1.50
4901AE	0.37	0.35	0.33
4911AE	0.37	0.35	0.33

### D.I.L. SOCKETS

	1	100	500+
8-pin	0.11	0.09	0.08
14-pin	0.13	0.11	0.10
16-pin	0.14	0.12	0.10
18-pin	0.15	0.13	0.11

### 7-SEGMENT DISPLAYS

	1	25	100+
0.3" DIL	0.90	0.80	0.75
Comm. Anode. 14-pin DIL. Red LED			

## SOLAR POWERED 100-Year Calendar Watch

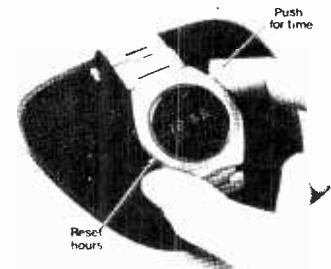


SP-1

This is the world's first solar-powered timepiece. Solar cells (similar to those used in the Skylab program) draw power from the sun (10 to 15 minutes per day) or from ambient light (slightly longer) to keep batteries fully charged. Batteries operate up to 10 years without replacement. A true calendar watch — LSI circuitry is programmed to provide a calendar to the year 2100, automatically adjusting for 30 and 31 day months, even leap years. Automatic brightness control adjusts LED for perfect viewing even in outdoors. Shows minutes and hours, counts out seconds or shows the date. Easily adjusts to reset hour or date without affecting calendar. Shock and water resistant. Accurate to 5 seconds per month. **£298.50.**

### PRECISION TIMEPIECE WITH

## Brilliant LED Display



Reset hours

Push for time

TYPE LED-2

Press the button and the time is visible, brilliantly displayed in large easily read LED numerals. Pulsating colon marks the passage of each second. Quartz crystal assures highest possible accuracy. Stainless steel, water resistant case with comfortable band. **£74.00.**



Reset minutes

All goods brand new, to full manufacturer's spec. No standard parts sold. Visitors welcome, by appointment. Colleges, Govt. and Account orders welcomed.

TERMS: Non-Account Customers, Cash with Order. Standard P&P 40p. Please add VAT to overall total.



# RASTRA ELECTRONICS LTD.

275-281 King Street · Hammersmith · London W6 9NF · Tel. 01-748 3143/2960 · Telex 24443





# VALVES

A1065	1.25	EF184	0.35
ARR	0.55	EF1200	0.75
ATP4	0.50	EL133	2.50
B13H	3.00	EL34	0.70
CY31	0.50	EL36	0.60
DAF96	0.50	EL41	0.80
DF96	0.55	EL81	0.60
DK96	0.55	EL82	0.55
DL92	0.40	EL84	0.30
DL96	0.60	EL85	0.60
DF96/B7	0.40	EL86	0.45
DY802	0.45	EL90	0.45
EB8CC/01120	0.40	EL504	0.80
E180CC	0.70	EM31	0.60
E182CC	1.25	FM80	0.55
EA50	0.40	EM84	0.40
EABC80	0.40	EM87	1.00
EAF42	0.75	EY51	0.45
EB91	0.30	EY81	0.45
EB93C3	1.00	EY86	0.40
EB94	0.75	EY88	0.50
EBF80	0.40	EZ40	0.70
EBF83	0.50	EZ41	0.75
EBF89	0.40	SC1/400	3.00
ECC52	0.35	EZ81	0.30
ECC81	0.40	GY501	0.75
ECC82	0.35	GZ34	0.70
ECC83	0.35	GZ37	1.00
ECC84	0.35	K166	2.50
ECC85	0.40	K189	3.20
ECC86	0.90	MM4	0.75
ECC88	0.50	ML6	0.65
ECC89	0.70	OA2	0.45
ECCF80	0.40	OB2	0.45
ECCF82	0.40	PABC80	0.40
ECCF81	0.75	PC37	0.50
ECH42	0.80	PC90	0.40
ECH81	0.35	PC84	0.40
ECH83	0.45	PC85	0.40
ECH84	0.45	PC89	0.50
ECL80	0.55	PC189	0.60
ECL82	0.35	PCF80	0.40
ECL83	0.70	PCF82	0.80
ECL86	0.50	PCF84	0.80
EF36	0.65	PCF86	0.60
EF37A	1.20	PCF200	0.75
EF40	0.75	PCF201	0.75
EF41	0.65	PCF801	0.55
EF80	0.30	PCF802	0.50
EF83	1.25	PCF805	0.80
EF85	0.35	PCF806	0.75
EF86	0.35	PCF808	0.90
EF89	0.30	PCF200	0.80
EF91	0.45	PC181	0.55
EF92	0.50	PC182	0.40
EF95	0.40	PC183	0.65
EF183	0.35	PC184	0.45

PCL86	0.50	Z801U	2.70	6AK5	0.40	6CL6	0.75	6X5GT	0.50
PCL805	0.60	Z900T	1.20	6AK8	0.40	606	0.55	6Y6G	0.90
PFL200	0.70	1A3	0.55	6AL5	0.30	6E8A	0.85	6Z4	0.85
PL36	0.60	1L4	0.25	6AL5W	0.55	6F7	1.10	630L2	0.90
PL81	0.50	3A4	0.60	6AM6	0.45	6FR6	0.75	7B7	0.80
PL82	0.45	1R5	0.40	6AN8	0.45	6FZ3	0.90	7Y4	0.80
PL83	0.45	1S4	0.30	6AX5	0.75	6F32	0.75	9D6	0.40
PL84	0.45	1T4	0.30	6AQ5W	0.70	6F33	3.50	9D7	6.00
						6H6	0.35	12A6	0.55
						6J4WA	1.25	12A6	0.45
						6J5	0.65	12A7	0.40
						6J5GT	0.50	12A7	0.35
						6J6	0.60	12A6V	0.50
						6J7	0.60		
						6J7G	0.40		
						6K6GT	0.80		
						6K7	0.55		
						6K7G	0.30		
						6K8GT	0.50		
						6K25	1.00		
						6L6	1.90		
						6L6G	0.60		
						6L7G	0.40		
						65A7	0.50		
						65A7GT	0.40		
						65H7	0.90		
						12C8	0.55		
						12E1	3.50		
						12K5	1.10		
						12K7GT	0.50		
						12K8GT	0.70		
						12Q7GT	0.70		
						12S4GT	0.70		
						12S7	0.55		
						12S7J	0.55		
						12Y4	0.40		
						14S7	1.00		
						19A05	0.65		
						19G3	8.00		
						19G6	6.60		
						19H5	14.00		
						20P3	6.00		
						20P4	1.10		
						25L6GT	0.70		

Many of these valves are imported and prices vary for each delivery so we reserve the right to change prices for new stock when unavoidable

PL504	0.80	1X2A	0.60	6AS6	0.80	6X5GT	0.50
PL508	1.00	1X2B	0.75	6AT6	0.45	6Y6G	0.90
PL509	1.35	2D21	0.50	6AU6	0.40	6Z4	0.85
PL512	0.95	2K25	9.00	6AV6	0.45	630L2	0.90
PY80	0.40	3D6	0.40	6AX4GT	0.75	7B7	0.80
PY81	0.40	3S4	0.40	6AX5GT	1.00	7Y4	0.80
PY82	0.40	3V4	0.85	6B7	0.70	9D6	0.40
PY83	0.40	5B/254M	4.50	6BA6	0.35	9D7	6.00
PY84	0.40	5B25M	3.50	6BE6	0.40	12A6	0.55
PY85	1.00	5R4GY	0.90	6BG6G	0.90	12A7	0.40
PY86	0.40	5U4G	0.50	6B6J	0.65	12A6V	0.50

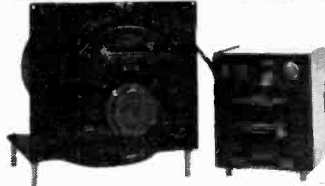
## VALVES AND TRANSISTORS

Telephone enquiries for valves, transistors etc. retail 749 3934; trade and export 743 0899

SV4G	0.55	6B07A	0.80	6SJ7GT	0.35	AC113	2.00
5Y3GT	0.55	6BR7	1.20	6SK7	0.55	AC126	2.00
5Z3	0.80	6BW6	1.00	6SL7GT	0.50	AC127	2.00
5Z4	0.80	6BW7	1.00	6SN7GT	0.50	AC128	2.00
5Z4TG	0.55	6C4	0.40	6S07	0.55	AC176	2.00
6A87	0.60	6C6	0.50	6V6GT	0.50	AC18	2.00
6AC7	0.60	6CB6	1.50	6X4	0.40	AC19	2.00
6AH6	0.70	6CH6	1.45	6X5G	0.40	AC20	2.00
						AC27	2.00
						AC28	2.00
						AC76	2.00
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						AC19	2.

# ELECTRONIC BROKERS

## SIGNAL SOURCES



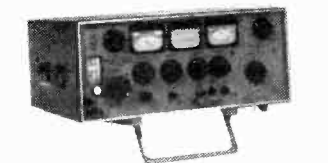
Unit Oscillator. General Radio Type 1209C. Freq. 250-920 MHz Accuracy 1% Drift 0.2%. Output into 50 ohms = 150 MW with PSU 1201 - CO18 as illustrated **£215**

**ADVANCE**  
Audio Signal Generator HIB 15Hz-50 KHz 200V-20V± 2dB Sine Wave & Square Wave **£65**  
Audio Signal Generator J18 15Hz-50KHz 0.2V-25V **£65**  
VHF Square Wave Generator SG 21 9KHz-100MHz Max 0/p 2V **£35**  
Signal Generator D1 **£39**  
**AIRMEC**  
Signal Generator 702 30Hz-30KHz in 3 bands **£60**  
Signal Generator 701 **£60**  
H.F. Signal Generator 201 30KHz-30MHz in 7 Bands Int.Xtal calibrator 0/p level variable 1µV-11V 75 ohms impedance Int. Mod. at 1KHz Ext. Mod 30Hz-10KHz **£75-£115**

**GENERAL RADIO**  
Unit Oscillator 1218-A P.O.A.  
**HEWLETT PACKARD**  
U.H.F. Signal Generator 614A 900-2100MHz 1% Accuracy Output 0.1µV-0.2V into 50 ohms Modulation CWInt or EXT FM & Pulse S.H.F. Signal Generator 618C 3.8-7.6GHz ± 1% 50 ohms **£550**  
Signal Generator 6088 10-400MHz 0.1µV-0.8V **£195**  
Signal Generator 612A 450MHz-1230MHz Internal & Ext. A.M. 50 ohms **£495**  
Audio Oscillator Type 201C 20 Hz-20 KHz 0.40 dB in 10 dB steps. Distortion less than 0.5%. Also 200 CD & 200B **£95**  
FM/AM Signal Generator 202H **£495**

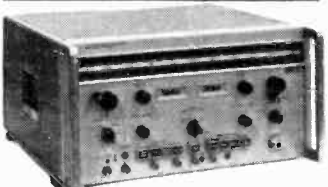
**MARCONI INTS.**  
Oscillator TF1247 20-300MHz (Suitable for use with Marconi TF 1245 & 1245A O-Meters) **£135**  
FM/AM Signal Generator TF 995A/3S 1.5 Mhz-220 MHz. 2µ V-200mV Superb condition **£385**  
U.H.F. Signal Generator TF 1060/2 450-1200 MHz 0.1µV-447mV Sine and pulse mod. facilities **£420**  
U.H.F. & S.H.F. Signal Generator TF 1058 1600-4000 MHz 0.1µV-445mV **£295**  
Signal Generator TF 867. 15 KHz-30 MHz 0.4µ V-4V. Int and ext mod facilities **£135**  
Phase/AM Signal Generator TF 2003 0.4-12 MHz Bargain price - super condition **£150**

**WAYNE KERR**  
Video Oscillator 0.22D 10 KHz-10 MHz **£150**  
A.F. Oscillator S121 10 Hz-120 KHz **£45**  
**BRUEL & KJAER**  
Portable Sound Level and Vibration Meter 2203 and Octave Filter Set 1613 **£275**  
Level Recorder 2305 P.O.A. **£395**  
S.E.U.V. Recorder 3006



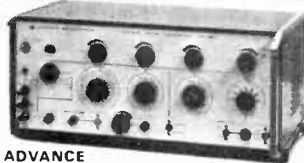
**HEWLETT PACKARD**  
Sweep Oscillator 692D 2-4GHz **£495**  
Sweep Oscillator 693B 4-8GHz **£495**  
**JERROLD**  
Sweep Signal Generator 900B Centre Freqs 500KHz-1200MHz Sweep widths narrow as 10KHz to 400MHz wide 50ohms

## SWEEP GENERATORS



**HEWLETT PACKARD**  
Sweep Oscillator 692D 2-4GHz **£495**  
Sweep Oscillator 693B 4-8GHz **£495**  
**JERROLD**  
Sweep Signal Generator 900B Centre Freqs 500KHz-1200MHz Sweep widths narrow as 10KHz to 400MHz wide 50ohms

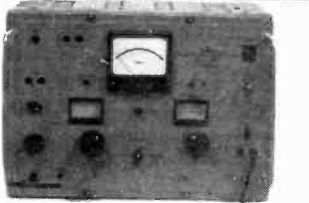
## PULSE GENERATORS



**ADVANCE**  
Double Pulse Generator PG 56 Pulse Amplitude 0.1V-10V Sq wave 0-10V Rise Time 10nsec (typically) **£87.50**  
Pulse Generator PG 55 P.O.A.  
Modular Pulse Generator Advance Type PG 52 System of 5 Signal generating & Processing units Repetition freqs up to 20MHz & Output pulses to 20V (50 ohms) Rise & Fall times 5nsec Its versatility enables the production of complex pulse & ramp waveforms not obtainable from conventional pulse generators **£250**

**MARCONI**  
Double Pulse Generator TF 1400 S. Min type CT 434 c/w TM 6600 Sec Pulse gen Plug In. 10Hz-100KHz 100nsec-100µsec Negative pulses up to 200V E.M.F. +VE pulses up to 60V E.M.F. & Simultaneous +VE & -VE pulses up to 20V E.M.F. P.O.A.  
**SOLARTRON**  
Precision Pulse Generator G.O 1377 100V single or double pulses 0.2 amp paraphase outputs Simultaneous +VE & -VE outputs. Square wave to 5MHz 10nsec Rise time Pulse repetition freq - 10Hz-1MHz Pulse duration 0.1µsec-100nsec **£125**  
Pulse Generator OPS 100C P.O.A.

## TELEPHONE TEST EQUIPMENT



Siemens Level Meter 3D 335 10KHz-17MHz Complete system by Siemens comprising 3W 518 Level Oscillator 3D 335 Level Meter. 3W 933 Sweep Attachment. 3D 346 Screen Level Tracing Receiver P.O.A.  
Siemens Level Meter 3D 332 0.3-1200KHz Level Oscillator 3W 29 0.3-1200KHz P.O.A. S.T.C.

Octave Filter 74143A 37.5-12.800Hz For analysing noise and interference on comms systems, particularly useful with 74142 psophometer P.O.A.  
Selective level Measuring Set 74184B 60-1364KHz P.O.A.  
Measuring Set 74831A P.O.A.

**A.T.&E.**  
Telegraph Distortion Measuring Set Various types 5BV 5BV3 6BV 6A P.O.A.  
**MURPHY RADIO**  
Receiver VHF field strength RX 506 & interference measuring set c/w Power Unit P.O.A.

## OSCILLOSCOPE TEST EQUIPMENT



**TEKTRONIX**  
Pulse Generator Type III 0.5µsec risetime Amplitude ± 5V 30 to 250 nsec difference between trigger and output pulses **£60**  
Time Mark Generator 180A **£85**  
Pulse Generator 109 0.25 nsec Risetime 0-55V Calibrated variable amplitude Impedance 50 ohms **£35**  
Pre-Trigger Pulse Generator III **£60**

## RESISTANCE & DECADE BOXES

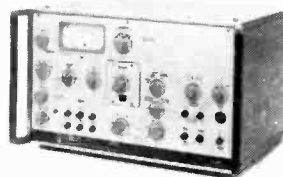


**MARCONI**  
Decade Potentiometer TF 221 **£40**  
Variable Air Condenser Muirhead Type 11-8 1250pF Max. P.O.A.  
AC-DC Converter Type AC-DC For use with Precision R Boxes **£90**

**NEGRETTI & ZAMBRA**  
Quick Reading Potentiometer **£55**  
Tinsley Vernier Potentiometer Type 3126B A precision equipment as used in laboratories and measurement standards areas **£125**

**DORAN**  
Whetstone Bridge Type 1401 **£45**  
Whetstone Bridge Type 3557 **£45**

## T.V. TEST EQUIPMENT



Wandel & Goltermann VZM 2 Distortion measuring set for phase & amplitude mod. For multichannel FM Radio Systems up to 12MHz Base bands **£400**

**MARCONI**  
Sine Squared Pulse & Bar Generator TF 2905/8 **£225**

**GRESHAM LION**  
Waveform Generator 625 lines Sine squared Pulse & Bar P.O.A.  
Waveform Generator 625 lines staircase P.O.A.

**MARCONI**  
Colour Gain & Delay Test Set TF 2904 **£275**  
**WANDEL & GOLTERMAN**  
Measuring Set VZM 1 **£495**  
Generator & Receiver VZM 83 **£275**

## COMPONENTS

Numeric Tube B 5853 0.9 Digit 1.4 height Brand New **£1.00**

Also Alpha Numeric Nixie Tube  
B.7971 Displays alphabet & 0-9 numerals **99p**

**ACCELEROMETERS**  
G.E.C. Type F **£2.50**  
Graseby Insts. Type 821 12G-0-12G **£25**  
Sperry Type 212502-0100 P.O.A. **£45**  
Sperry Type 214202-0100 P.O.A. **£25**  
Langham Thompson LA 2 Types up to 100G Choppers - **£4**  
Ericsson N 29834Hz **£4**  
Elliott Synchroverter G 1280 **£4**  
Elliott Synchroverter 95908 **£4**

**MODULATORS**  
S.E. Labs SE 441/2 **£45**  
S.E. Labs SE 501/2 **£45**  
Osc. amp. demod. SE Labs Type SE 62/12 4000 p.s.i. **£85**

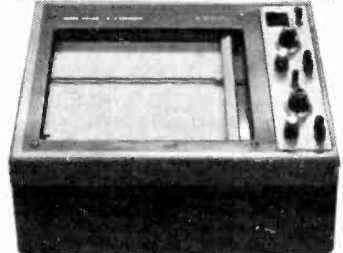
**TRANSDUCERS**  
S.E. Labs SE 150T 2.5 p.s.i. **£35**  
S.E. Labs SE 153 A7481 15 p.s.i. **£35**  
S.E. Labs SE 250 A5962 1000 p.s.i. **£25**  
S.E. Labs SE 150B 50 p.s.i. **£35**  
S.E. Labs SE 105 1000 p.s.i. **£25**  
S.E. Labs SE 165 4000 p.s.i. **£25**

**TEMPERATURE INDICATORS**  
Made by Ether. Models with Temp Ranges 0-600 C 0-800 C & 0-1000 C **£25-£50**

**POTENTIOMETERS**  
3 turn and 5 turn available 10 turn 3600 Rotation

5 ohms	Beckman	Type A	£3 00
50 ohms	Bourns	35005-2-500	£1 00
100 ohms	Relcon	05 B10	£1 00
300 ohms	Beckman	7216	£2 50
500 ohms	Beckman	A	£2 50
500 ohms	Colvern	2501/264	£3 00
500 ohms	Colvern	2402/13	£3 00
500 ohms	Colvern	2501/9	£3 00
500 ohms	Relcon	07-10	£2 50
1K	Beckman	as 690	£3 00

## X-Y & U/V RECORDERS

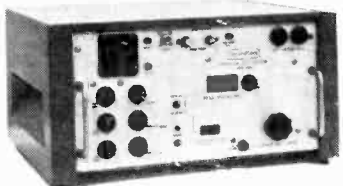


X-Y Recorder Advance Type HR 96 **£195**  
**ADVANCE**  
X-Y Recorder HR. 92/1 **£150**  
**BELL & HOWELL**  
U.V. Recorder 5/127, without Galvo s **£225**  
**BRYANS**  
X-Y Recorder 20021 **£195**  
**ELECTRONIC ASSOCIATES**  
Vari-Plotter **£145**

## INSULATION TESTERS

**EVERSHED & VIGNOLES**  
Circuit Tester Ohmmeter 0-3 ohms 0-39 ohms **£18**  
Circuit Tester Ohmmeter 0-1000 ohms 100-200 kohms **£18**  
Megger Series 4-II 250V **£12**  
Megger Series III Mk 3 250V **£20**  
Megger 250V **£20**  
Megger 500V **£37**  
Battery Megger 500V **£37**  
**PYE**  
Insulation Tester 108 500V **£25**

## MISCELLANEOUS



Transfer Oscillator Type 7580HBy Beckman DC 15GHz with counter 7.5MHz-15GHz without counter Sensitivity 100mV (R.M.S.) **£350**

**MARCONI**  
Distortion Factor Meter TF 142F Fundamental Freq. Range 100Hz-8KHz Dist measurement ranges 0-5% & 0-50% **£60**  
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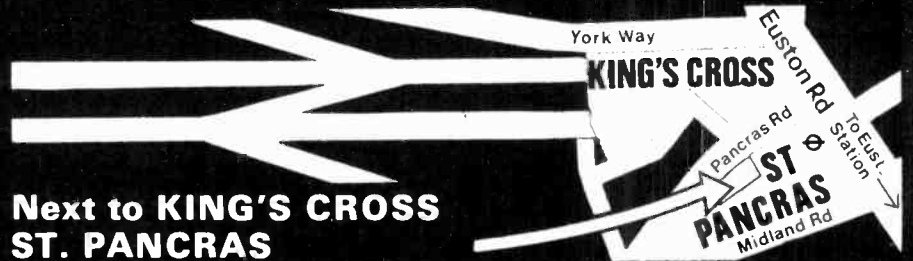
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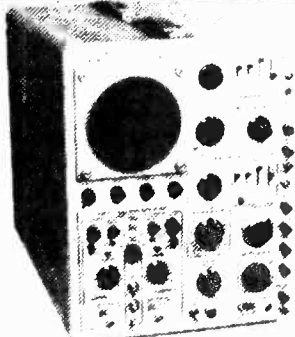
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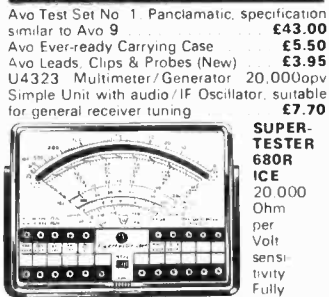
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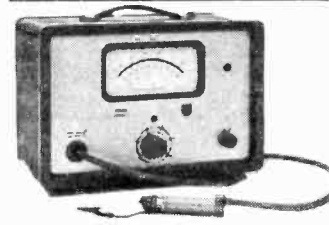
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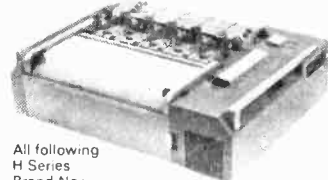
## DIGITAL VOLTMETERS



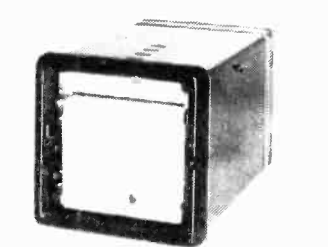
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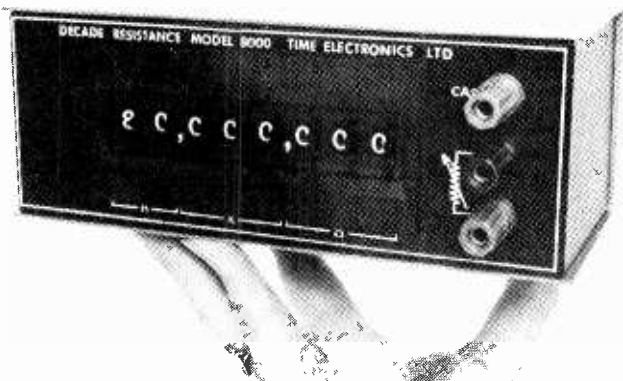
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0B2	0.47	6BA6	0.41	6L6GC	0.68	12AV6	0.59	30P4MR	AL60	1.17	E8L21	2.34	EV31	0.52	UY41	0.53	AF121	0.39	BVZ13	0.33	OA211	0.86
0Z4	0.55	6BC8	0.70	6L7(M)	0.59	12AX7	0.39	30P12	AL70	0.70	E8L41	0.70	EV32	0.53	UY42	0.53	AF124	0.33	BVZ15	0.33	OC19	1.62
1A3	0.53	6BE6	0.41	6L8	0.64	12AY7	0.94	30P12	ATP4	0.59	EC53	1.17	EM81	0.87	UY85	0.22	AF125	0.22	CG12E	0.26	OC22	0.49
1ASGT	0.59	6BG6G	1.23	6L19	2.34	12BA6	0.53	30P19	AZ1	0.29	FC54	1.17	EM82	1.12	UY10	1.17	AF126	0.23	CG64H	0.26	OC23	0.49
1ATGT	0.76	6BH6	0.70	6L1D12	0.45	12BE6	0.59	30P4	AZ31	0.70	FC66	0.82	EM83	0.64	UY12	1.17	AF129	0.84	FSY11A	0.29	OC24	0.49
1B3GT	0.59	6BK6	0.64	6LD20	0.88	12BH7	0.59	30P11	BL1	0.29	FC88	0.82	EM84	0.76	UY16	1.17	AF138	0.84	FSY41A	0.29	OC25	0.49
1C2	0.82	6BK7A	0.70	6N7GT	0.70	12B7V	0.88	30P13	BL21	0.29	FC88	0.82	EM85	0.76	UY17	0.88	AF140	0.62	GD4	0.42	OC28	0.77
1G6	1.17	6BQ5	0.36	6PL12	0.40	12E1	3.51	30P14	CL33	1.87	FC32	1.76	EV31	0.47	UY20	1.17	AF156	0.71	GD5	0.36	OC29	0.81
1HSGT	0.70	6BQ7A	0.64	6P15	0.36	12S1GT	0.39	30P15	CV6	0.62	FC33	1.76	EV32	0.47	UY23	2.93	AF159	0.49	GD6	0.36	OC36	0.55
1L4	0.33	6BR7	1.17	6Q7G	0.59	12J7GT	0.70	35A3	CV63	0.88	FC33	1.76	EV33	0.47	UY24	0.88	AF160	0.62	GD4	0.42	OC38	0.77
1LD5	0.70	6BR8	1.76	6Q7GT	0.59	12K5	1.17	35C5	CV988	0.29	EC40	1.17	EV37	0.63	UY28	1.17	AF166	0.71	GD5	0.36	OC39	0.81
1LNS	0.70	6BS7	1.64	6Q7(M)	0.64	12K7GT	0.59	35D5	CY1C	1.17	EC81	0.40	EV38	0.47	UY30	1.17	AF179	0.49	GD6	0.36	OC38	0.55
1NSGT	0.76	6RW6	0.94	6R7G	0.70	12Q7GT	0.53	35L6GT	CY31	0.59	EC82	0.39	EV39	0.68	UY32	0.88	AF180	0.52	GD8	0.26	OC38	0.55
1RS	0.53	6BW7	0.82	6R7(M)	0.68	12Q7GT	0.53	35W4	D63	0.29	FC83	0.39	EV35	0.53	UY37	2.05	AF182	0.47	GD9	0.26	OC41	0.64
1S4	0.39	6BK6	0.29	6SA7	0.52	12S7	0.59	35Z3	DAC32	0.70	EC84	0.41	EZ40	0.59	UY38	0.76	AF183	0.20	GD11	0.26	OC42	0.81
1S5	0.35	6BY7	0.35	6SC7GT	0.39	12S7GT	0.47	35Z4GT	DAF96	0.59	EC85	0.47	EZ41	0.64	UY41	0.76	AF184	0.20	GD12	0.26	OC43	1.52
1U4	0.70	6BZ6	0.57	6SG7	0.52	12SH7	0.41	35Z5GT	DC90	0.70	EC86	1.00	EZ40	0.33	UY42	1.76	AF185	0.18	GD14	0.64	OC44	0.13
1U5	0.88	6C4	0.47	6SH7	0.52	12S17	0.52	42	DD4	1.17	EC88	0.52	EZ41	0.33	UY43	0.84	AF186	0.21	GD5	0.36	OC45	0.14
2D21	0.53	6CSG	0.59	6S4	0.64	12SK7	0.64	38B5	DF91	0.40	FC189	0.76	EZ40	0.47	UY44	1.17	AF187	0.18	GD6	0.36	OC46	0.20
2X2	0.64	6C6	0.47	6SK7GT	0.52	12SN7GT	0.70	50C5	DF96	0.59	EC804	0.70	F4	1.17	UY45	1.17	AF188	0.18	GD13	0.64	OC65	1.45
2GK5	0.70	6C9	1.17	6SQ7GT	0.53	0.70	50C6DG	1.46	DH63	0.59	EC807	0.70	FC4	1.17	UY47	0.70	AF189	0.20	GD16	0.26	OC46	0.20
3A4	0.59	6C86A	0.47	6U4GT	0.82	12SQ7GT	0.70	50F5H	DH76	0.53	EC80	0.53	FC4	1.17	UY49	0.76	AF190	0.20	GD17	0.26	OC67	1.14
3B7	0.53	6C12	0.39	6U7G	0.53	0.76	50L6GT	0.76	DH77	0.53	EC82	0.53	FC4	1.17	UY50	0.76	AF191	0.20	GD18	0.26	OC72	0.14
3D6	0.47	6C17	2.34	6V6G	0.20	12SR7	0.88	72	DH81	0.88	EC86	0.88	FC4	1.17	UY51	0.82	AF192	0.20	GD19	0.26	OC73	0.29
3Q4	0.70	6C24	0.70	6V6GT	0.53	14H7	0.64	77	DD32	0.76	EC87A	0.88	FC4	1.17	UY52	0.82	AF193	0.20	GD20	0.26	OC74	0.29
3QSGT	0.64	6C8GA	0.88	6X4	0.47	14S7	0.84	85A2	GZ0	0.30	EC88	0.52	GZ30	0.53	UY53	0.82	AF194	0.20	GD21	0.26	OC75	0.14
3S4	0.47	6C16	0.76	6X5GT	0.53	1.17	85A3	0.70	DK92	0.82	EC821	2.34	GZ32	0.59	UY54	0.82	AF195	0.20	GD22	0.26	OC76	0.20
3V4	0.82	6CL8A	0.94	6Y6G	0.94	19A05	0.59	90A9	DK96	0.70	EC835	1.46	GZ33	1.46	UY55	0.82	AF196	0.20	GD23	0.26	OC77	0.35
4CB6	0.64	6CM7	0.88	6Y7G	1.17	19B6G6	0.90	90C9	DL92	0.47	EC842	2.63	GZ34	0.70	UY56	0.82	AF197	0.20	GD24	0.26	OC78	0.20
5C68	0.64	6C05	0.88	7A7	1.17	1.17	90CV	2.81	DL94	0.82	EC848	0.82	GZ37	1.17	UY57	0.82	AF198	0.20	GD25	0.26	OC79	0.52
5R4GY	0.94	6CW4	1.17	7B6	0.88	19G6	7.02	90C1	DL96	0.64	EC848	0.82	GZ37	1.17	UY58	0.82	AF199	0.20	GD26	0.26	OC81	0.14
5TA	0.47	6D3	0.70	7B7	0.82	19H1	2.34	150B2	DM70	0.70	EC864	0.52	HAB80	0.70	UY59	0.82	AF200	0.20	GD27	0.26	OC82	0.29
5U4G	0.47	6D7	0.88	7F8	1.76	20D1	0.70	2155G	DM71	1.76	EC80	0.47	HL13C	0.59	UY60	0.82	AF201	0.20	GD28	0.26	OC83	0.29
5V4G	0.59	6DT6A	0.88	7H7	0.88	20D4	2.34	301	DM74	0.82	EC82	0.40	HL13D	0.70	UY61	0.82	AF202	0.20	GD29	0.26	OC84	0.14
5Y3GT	0.53	6EW6	0.88	7R7	0.82	20P2	0.88	302	DW4/350	1.17	EC83	0.82	HL23DD	0.70	UY62	0.82	AF203	0.20	GD30	0.26	OC85	0.14
5Z3	0.88	6E5	1.17	7V7	1.76	20L1	1.29	303	DY87/6	0.41	EC84	0.70	HL30	0.88	UY63	0.82	AF204	0.20	GD31	0.26	OC86	0.14
5Z4G	0.53	6F1	0.88	7Y4	0.88	20P1	0.64	305	DY802	0.41	EC85	0.70	HL41	1.17	UY64	0.82	AF205	0.20	GD32	0.26	OC87	0.14
5Z4GT	0.53	6F6G	0.59	7Z4	0.94	20P3	0.84	307	EM0CC	2.57	EC86	0.47	HL41D	1.17	UY65	0.82	AF206	0.20	GD33	0.26	OC88	0.14
6/30L2	0.70	6F12	0.43	9BW6	0.82	20P4	1.17	956	E80F	1.64	EC87	1.76	HL42	2.34	UY66	0.82	AF207	0.20	GD34	0.26	OC89	0.14
6A8G	1.46	6F13	0.82	9D7	0.76	20P5	1.52	1821	E83F	1.52	EC88	0.47	HL42DD	2.34	UY67	0.82	AF208	0.20	GD35	0.26	OC90	0.14
6A7C	0.57	6F14	0.88	10C2	0.76	25A6G	0.70	4033X	E88CC	0.88	EC89	0.47	HL43	2.34	UY68	0.82	AF209	0.20	GD36	0.26	OC91	0.14
6AG5	0.32	6F15	0.76	10D1	0.82	25L6G	0.70	5702	E92CC	0.70	EC90	0.47	HL44	2.34	UY69	0.82	AF210	0.20	GD37	0.26	OC92	0.14
6AH6	0.70	6F18	0.46	10E7	0.88	25V5	0.84	5763	F1R0CC	0.82	EC91	0.47	HL45	2.34	UY70	0.82	AF211	0.20	GD38	0.26	OC93	0.14
6A15	0.76	6F23	0.82	10F1	0.88	25V5G	0.82	6057	F1R0F	1.17	EC92	0.47	HL46	2.34	UY71	0.82	AF212	0.20	GD39	0.26	OC94	0.14
6A18	0.39	6F24	1.00	10F3	1.17	25Z4G	0.47	6080	F1R2C	1.46	EC93	0.47	HL47	2.34	UY72	0.82	AF213	0.20	GD40	0.26	OC95	0.14
6AK5	0.47	6F25	1.17	10F9	0.76	25Z5	0.94	6067	F1L14	0.82	EC94	0.47	HL48	2.34	UY73	0.82	AF214	0.20	GD41	0.26	OC96	0.14
6AK6	0.70	6F26	0.35	10F18	0.64	25Z6G	0.82	7193	EASO	0.32	EC95	0.47	HL49	2.34	UY74	0.82	AF215	0.20	GD42	0.26	OC97	0.14
6AK8	0.45	6F28	0.78	10L14	0.53	28D7	1.17	7475	EAB7E	1.17	EC96	0.47	HL50	2.34	UY75	0.82	AF216	0.20	GD43	0.26	OC98	0.14
6AL5	0.23	6F32	0.59	10LD11	0.82	30A5	0.76	9002	EAC80	0.88	EC97	0.47	HL51	2.34	UY76	0.82	AF217	0.20	GD44	0.26	OC99	0.14
6AM8A	0.64	6G6G	0.59	10LD12	20.47	30C1	0.47	9006	EC91	0.45	EC98	0.47	HL52	2.34	UY77	0.82	AF218	0.20	GD45	0.26	OC100	0.14
6AN8	0.82	6CH8A	0.88	10P12	0.45	30C5	0.82	A1834	EC92	1.17	EC99	0.47	HL53	2.34	UY78	0.82	AF219	0.20	GD46	0.26	OC101	0.14
6AQ5	0.53	6C15	0.76	10P13	0.88	30C7	0.84	A2134	FAF42	0.88	EC99	0.47	HL54	2.34	UY79	0.82	AF220	0.20	GD47	0.26	OC102	0.14
6AQ8	0.47	6G7U	0.88	10P14	2.34	30C8	0.82	A3042	FAE801	0.88	EC98	0.47	HL55	2.34	UY80	0.82	AF221	0.20	GD48	0.26	OC103	0.14
6AR5	0.70	6H6GT	0.29	10P18	0.49	30F5	0.88	AC2PEN	EB34	0.29	EC98	0.35	KTW62	1.17	UY81	0.82	AF222	0.20	GD49	0.26	OC104	0.14
6AR6	1.17	6J5GT	0.53	12A6	1.17	30F11	0.78	AC2PENDD	EB91	0.23	EC98	0.41	KTW62	1.17	UY82	0.82	AF223	0.20	GD50	0.26	OC105	0.14
6AS7	1.17	63C	0.35	12AC6	0.82	30FL2	0.78	AC2PENDD	FBC41	0.88	EC98	1.46	MH14	0.82	UY83	0.82	AF224	0.20	GD51	0.26	OC106	0.14
6AT6	0.53	617G	0.35	12D6	0.76	30FL12	1.05	AC6/PEN	FBC81	0.88	EC99	0.53	MH16	1.17	UY84	0.82	AF225	0.20	GD52	0.26	OC107	0.14
6AU6	0.53	617(M)	0.53	12A6E	0.76	30FL13	0.64	AC6/PEN	EB90	0.35	EC90	0.41	MKT4	1.17	UY85	0.82	AF226	0.20	GD53	0.26	OC108	0.14
6AV6	0.53	6J0A	0.88	12A76	0																	



TRANSISTORS						I.C.s 74 SERIES						JETS SUPER BARGAIN PACKS							
AC107	0.16	BC158	0.11	CV7464	0.10	2G106	0.21	SN7400	0.14	SN7413	0.30	SN7442	0.73	SN7497	0.75	No.	Ctry.	Contents	Price
AC126	0.16	BC159	0.13	CV7594	0.25	2G306	0.44	SN7401	0.14	SN7416	0.30	SN7450	0.15	SN7493	0.73	J1		1 Pre-amp component kit plus data	0.65
AC127	0.16	BC171	0.16	CV7648	0.30	2G345A	0.18	SN7402	0.14	SN7417	0.29	SN7460	0.15	SN7494	0.80	J2		3 Transistors AF115 new and marked	0.65
AC128	0.12	BC172	0.16	CV8762	0.40	2G402	0.25	SN7403	0.14	SN7423	0.40	SN7472	0.30	SN74121	0.49	J4		4 Transistors 2N726 new and marked	0.65
AC138	0.20	BC173	0.18	MOS33	0.30	2N526	0.16	SN7404	0.14	SN7425	0.39	SN7473	0.41	SN74122	0.70	J5		8 Zener diodes top hat type 7.5 volt	0.65
AC141	0.20	BC184	0.18	MJE4102	0.12	2N697	0.15	SN7405	0.15	SN7430	0.14	SN7474	0.40	SN74123	0.70	J7		50 Metres con/wire mixed colours	0.65
AC142	0.20	BC208	0.12	MJE2021	0.85	2N715	0.35	SN7406	0.39	SN7432	0.39	SN7476	0.42	SN74151	1.05	J8		25 Metres con/wire 4 Metres 60/40 solder	0.65
AC153	0.22	BC209	0.13	MJE2955	0.95	2N726	0.25	SN7407	0.37	SN7433	0.40	SN7480	0.16	SN74153	0.95	J9		100 Resistors HI/STAB 1/4w mixed values	0.65
AC154	0.22	BC212L	0.14	MJE3055	0.60	2N753	0.55	SN7408	0.26	SN7440	0.15	SN7486	0.34	SN74195	1.07	J10		100 Resistors HI/STAB 1/4w mixed values	0.65
AC167	0.21	BC213L	0.12	NKT1162	0.25	2N1303	0.16	SN7409	0.23	SN7441	0.70	SN7490	0.50	SN74196	1.20	J12		250 Resistors mixed values	0.65
AC168	0.27	BC214L	0.14	NKT1164	0.25	2N1304	0.19	<b>930 SERIES LOGIC I.C.s</b>						MC948	0.25	J14		100 Capacitors miniature mixed values	0.65
AC169	0.16	BC301	0.30	NKT1212	0.20	2N1305	0.19	MC930	0.15	MC933	0.15	MC945	0.30	MC962	0.15	J15		5 Terminal blocks brand new 12 way	0.65
AC176	0.15	BC337	0.15	NKT221	0.17	2N1309	0.25	MC932	0.15	MC944	0.16	MC946	0.14	MC9093	0.40	J18		12 Standard crocodile clips	0.65
AC176	MP	BC211	0.28	NKT224	0.15	2N1754	0.30	SN741	0.35	SN76115	1.20	TCA270B	3.00	MC1103L	1.50	J19		12 Screwdrivers 5 inches long	0.65
AC128	0.25	BD131	0.40	NKT270	0.15	2N2484	0.30	LM380N	0.95	LM1310	1.25	<b>TESTED S.C.R.s</b>				J20		1 Pack nuts & bolts self tappers, etc.	0.65
AC177	0.26	BD132	0.40	NKT278	0.15	2N2923	0.16	<b>TESTED S.C.R.s</b>				J22		20 Volume controls lin & log mixed values	0.65				
AC178	0.25	BD131	MP	OC22	0.50	2N2924	0.18	50 PIV 1AMP TO-5 CASE 0.26	50 PIV 3AMP TO-66 CASE 0.29	J23		75 Syn/rubber grommets mixed sizes	0.65						
ACV17	0.28	BD132	0.75	OC28	0.80	2N2925	0.15	100 PIV 1AMP TO-5 CASE 0.31	100 PIV 3AMP TO-66 CASE 0.29	J26		20 Screw on rubber feet 1/4inch dia approx	0.65						
ACV18	0.22	BD139	0.70	OC35	0.45	2N2926	0.14	200 PIV 1AMP TO-5 CASE 0.32	200 PIV 3AMP TO-66 CASE 0.35	J26		1 Pack marker sleeve mixed colours & sizes	0.65						
ACV19	0.22	BD140	0.70	OC36	0.55	2N2926Y	0.12	400 PIV 1AMP TO-5 CASE 0.37	400 PIV 3AMP TO-66 CASE 0.47	J27		5 lengths ferrite rod mixed flat & round	0.65						
ACV20	0.20	BD243	0.85	OC44	0.17	2N2926R	0.11	600 PIV 1AMP TO-5 CASE 0.49	600 PIV 3AMP TO-66 CASE 0.57	J28		20 Tag strips assorted lengths	0.65						
ACV21	0.18	BD244	0.85	OC45	0.14	2N2926O	0.11	800 PIV 1AMP TO-5 CASE 0.78	800 PIV 3AMP TO-66 CASE 0.70	J29		4 Micro switches brand new	0.65						
ACV27	0.20	BF167	0.24	OC70	0.11	2N2926B	0.11	<b>THYRISTOR BT109 CON/BRI</b>				J29		20 Preset pots lin & log mixed	0.65				
ACV28	0.22	BF181	0.33	OC71	0.11	2N3053	0.19	<b>BRIDGE RECTIFIERS</b>				J32		20 Capacitors can type mixed values	0.65				
AD140	0.53	BF182	0.40	OC72	0.15	2N3054	0.50	50 RMS PLASTIC CASE 0.40	<b>OPTOELECTRONICS</b>				J33		50 Ceramic plate capacitors mixed values	0.65			
AD142	0.53	BF183	0.40	OC81	0.17	2N3055	0.50	100 RMS PLASTIC CASE 0.45	ORP 12 BRAND NEW	0.58	J34		1 Pack copper clad paxolin board	0.65					
AD149	0.55	BF194	0.12	OC200	0.28	2N3702	0.12	200 RMS PLASTIC CASE 0.49	ORP 60 BRAND NEW	0.56	J35		20 Fuse holders mixed	0.65					
AD161	0.43	BF195	0.30	OC201	0.32	2N3703	0.12	400 RMS PLASTIC CASE 0.52	OCF 71 BRAND NEW	0.54	J36		8 Metres multi/core solder 60/40 22swg	0.65					
AD162	0.43	BF196	0.15	OC202	0.27	2N3704	0.14	<b>UJT 2N6027 BRAND NEW</b>				J37		10 3.5mm Jack sockets chrome	0.65				
AD161	MP	BF197	0.16	OC203	0.29	2N3705	0.13	<b>ELECTROLYTICS 0.02/250v 4 0/64v 4 7/16v 6 8/40v</b>				J38		8 Sockets 5 pin & 2 pin	0.65				
AD162	0.85	BF200	0.50	OC204	0.28	2N3707	0.14	10/35volt 33uF/35v 40uF/16v ALL ONE PRICE 0.7 each	<b>TRIAIC 6AMP 400v CASE 66</b>				J39		2 Relays 12 & 24 volt	0.65			
AF115	0.26	BF234	0.39	OC445K	0.20	2N3710	0.10	47uF/35v 100uF/10v 0.8 each 125uF/16v 220uF/40v 680	<b>0.85</b>				J40		1 Pack of component boards ICs Transistors etc	0.65			
AF116	0.26	BU105	2.00	SGS26920	1.15	2N3711	0.10	uF/16v 6.3v/1500uF 0.12 each 16.16uF/500V 32.32uF/275v	<b>0.25 each 32.32uF/450v 0.35 each BARGAIN PRICES.</b>				<b>J PACKS ONLY ADD 10% TO TOTAL ORDER PLEASE FOR POST &amp; PACK</b>						
AF124	0.33	BFX29	0.28	SGS26942	1.14	2N3713	1.20	<b>POLYCARBONATE. 0.01uF/250v 0.033uF/250v10uF/250v</b>				<b>PAPST TAPE MOTOR 220v 50HZ E.50 p&amp;p 25p</b>							
AF125	0.31	BFX84	0.33	SGS26949	1.15	2N3094	0.33	0.1uF/250v 0.22uF/250v all 0.5 each. 1uF/250v 0.12 each.	<b>0.03 each QUOTATION GIVEN FOR 1000 of</b>				<b>AMPLIFIER 9 volt 500 Mw 0.95 p&amp;p 10p</b>						
AF178	0.50	BFX85	0.33	SGS27022	1.18	2N3905	0.31	<b>POLYESTER 0.0015/400v 0.022/160v 0.22/250v 6 8/400v</b>				<b>TELEPHONE DIALS BRAND NEW £1.00 p&amp;p free</b>							
ASV51	0.26	BFY50	0.20	SU203	0.65	2N3905	0.30	<b>METALISED FILM CAPACITORS. 0.047uF/250v 0.15/250V</b>				<b>P.A.R. BISTABLE RELAY LATCHING 24v DC4 C/O CONTACTS</b>							
BC107	0.11	BFY52	0.16	TK100	0.75	2N3908	0.30	<b>0.04 each</b>				<b>0.55</b>							
BC108	0.11	BFY81	0.65	THS91M	0.33	2N4059	0.15	<b>CAPACITORS 0.0015/350v 0.0047/500v 0.047/400V</b>				<b>RELAY T.M.C. MINIATURE 3 300 ohms 2 pole 4 way 0.55</b>							
BC109	0.11	BSY38	0.20	TK217	0.30	2N4287	0.20	<b>1uF/180v 0.25uF/250v 125uF/10v all 0.05 each</b>				<b>RELAY T.M.C. MINIATURE 3 300 ohms 2 pole 4 way 0.55</b>							
BC142	0.30	BSY39	0.20	V405A	0.25	2N4289	0.20	<b>SPECIAL OFFER I.C.s</b>				<b>SWITCH 4 POLE 2 CHANGE/OVER 0.15.</b>							
BC143	0.30	BSY40	0.31	V10/50	0.40	2N4291	0.22	<b>BULK PURCHASE</b>				<b>OUR BONAZZA CAPACITORS PACK IS STILL AVAILABLE ONLY £1.50</b>							
BC147	0.10	BSY41	0.31	Z116	0.75	2N4293	0.19	<b>BRAND NEW 14 PIN</b>				<b>100 MIXED VALUES &amp; TYPES VALUED AT OVER £5 (LATEST TYPES)</b>							
BC148	0.10	C111	0.50	ZTX107	0.12	25322	0.48	<b>OECADE COUNTERS 2</b>				<b>TWIN V/U METERS PLASTIC APPROX 40mm BY 80mm BRAND</b>							
BC149	0.10	C111E	0.55	ZTX302	0.17	25712	0.46	<b>SN7290 FOR ONLY</b>				<b>NEW READS 20 TO 1 MINUS ZERO TO 3 PLUS. L/R BARGAIN ONLY</b>							
BC157	0.11	CV5441	0.20	ZTX502	0.17	25745	0.45	<b>£1.00.</b>				<b>£2.95.</b>							
<b>DIODES</b>						<b>SPECIAL OFFER RESISTORS</b>						<b>MINIATURE EDGE LEVEL METER LOTS OF USES ONLY 0.95</b>							
AA119	0.06	BY127	0.12	OA202	0.07	IN4003	0.05	<b>CARBON FILM CR 75 TYPE 1M2. 2M2.</b>				<b>FREE OFFER ONE J PACK OF YOUR OWN CHOICE WITH ALL ORDERS</b>							
2/AA119	0.09	BY164	0.38	IN34A	0.08	IN4004	0.06	<b>10% 10 120 470K etc 200 mixed for only</b>				<b>VALUED AT OVER £5</b>							
AA215	0.11	BYX38/300	IN202	0.09	IN4005	0.07	<b>£1.25.</b>				<b>PLEASE ADD 10p MIN. TO ALL ORDERS WHERE NOT STATED</b>								
BA30	0.10	BY2213	0.46	IN252	0.19	IN4006	0.08	<b>LOW LOSS CO/AX CABLE 17p A METRE TWIN SPEAKER CABLE 8p</b>				<b>VAT INCLUDED AT CURRENT RATE</b>							
BA111	0.18	BY2213	0.28	IN914	0.06	IN4007	0.09	<b>A METRE</b>				<b>OVERSEAS POST AT COST</b>							
BA112	0.18	BZY95	0.15	IN984B	0.10	IN4151	0.06					<b>MAIL ORDER DEPT. ONLY</b>							
BAX7B/1	0.10	OA10	0.12	IN1124	0.09	IN4148	0.04					<b>(Callers by appointment)</b>							
BAY31	0.14	OA47	0.10	IN3064	0.10	IN4244	0.07					<b>J.E.T. ELECTRONICS</b>							
BAY74	0.12	OA81	0.08	IN4001	0.05	IS3036A	0.15					<b>90A MAWNEY ROAD, ROMFORD, ESSEX RM7 7DA</b>							
<b>ZENER DIODES</b>						<b>SPECIAL OFFER</b>						<b>SPECIAL OFFER</b>							
<b>400 mW 2.33v ALL 0.9 each</b>						<b>10 2N6027 P U T</b>						<b>10 2N6027 P U T</b>							
<b>1Watt 1.5 &amp; 2.33v ALL 0.19 each</b>						<b>FOR ONLY £1.25.</b>						<b>FOR ONLY £1.25.</b>							

# 8 DECADE RESISTANCE BOX



TIME ELECTRONICS LTD.  
Botany Industrial Estate  
Tonbridge Kent  
Tel. Tonbridge (07322) 5993, 3 lines

- ★ 1Ω -100MΩ
- ★ 0.1% Accuracy
- ★ Colour coded digits, Ω yellow, KΩ white, MΩ red.

WW—083 FOR FURTHER DETAILS

## INDUSTRIAL PRICES FOR THE HOBBYIST ALL 'BIG NAME' BRANDED GOODS SAME DAY SERVICE MONEY BACK GUARANTEE

LINEAR 1/C'S	DIODES	ZENER DIODES	
709C 0.24	IN4001 4	BZY88 400mW	
710C 0.24	IN4002 4	Voltagess 3.3v—30v	
741C (8P in Minidip) 0.20	IN4003 5	6p	
CA3046 0.50	IN4004 5	<b>AUDIO 1/C'S</b>	
LM309K 1.25	IN4005 6	IN4006 6	TAA661B 1.0
<b>COS/MOS</b>		IN4006 6	CA3089E 1.5
CD4001 0.24	IN914 2	OA47 4	CA3090Q 3.0
CD4009 0.40	OA47 4	OA200 6	CA3028 1.0
CD4011 0.20	OA200 6	IN4148 1.5	CA3048 2.0
CD4012 0.20	IN4148 1.5		
CD4018 1.80			
CD4029 1.50			
TRANSISTORS			
BC107 0.07	BFY50 0.14	2N696 0.15	
BC108 0.07	BFY51 0.12	2N697 0.20	
BC109 0.07	BFY52 0.15	2N706 0.10	
BCY70 0.09	BFY90 0.60	2N930 0.18	
BCY71 0.09	BSY95A 0.10	2N1302 0.16	
BCY72 0.09	C426 0.28	2N1303 0.12	
BFX29 0.16	40360 0.40	2N1304 0.20	
BFX84 0.16	40361 0.40	2N1305 0.20	
BFX85 0.16	40362 0.40	2N2160 0.50	
BFX86 0.16	40669 0.80	2N2646 0.40	
BFX87 0.16	40673 0.50	2N3053 0.15	
BFX88 0.16	40602 0.40	2N3054 0.40	
BC237 0.08		2N3055 0.40	

TERMS: CWO—10p POST & PACKING—ADD 25% VAT

### ROWNSGEM LTD.

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THE PROFESSIONAL ORGANISATION FOR THE 'HOBBYIST'



# Samson's

(ELECTRONICS) LTD.

9 & 10 CHAPEL ST., LONDON, N.W.1  
01-723 7851 01-262 5125

ADJACENT TO EDGWARE ROAD MET. LINE STATION

## CURRENT RANGE OF NEW L.T. TRANSFORMERS FULLY SHROUDED TERMINAL BLOCK CONNECTIONS ALL PRIMARIES 220/240V

Type	Sec Taps	Amperes	Price	Postage
1A	25:33-40-50v	15	<b>£15.50</b>	£1.00
1B	25:33-40-50v	10	<b>£13.25</b>	£1.00
1C	25:33-40-50v	6	<b>£9.50</b>	85p
1D	25:33-40-50v	3	<b>£8.25</b>	85p
2A	4:16-24-32v	12	<b>£11.25</b>	£1.00
2B	4:16-24-32v	8	<b>£8.75</b>	85p
2C	4:16-24-32v	4	<b>£5.25</b>	65p
2D	4:16-24-32v	2	<b>£3.85</b>	60p
3A	24-30-36v	10	<b>£10.00</b>	85p
3B	24-30-36v	5	<b>£8.25</b>	65p
3C	24-30-36v	2	<b>£3.85</b>	60p
4A	12-20-24v	20	<b>£13.25</b>	£1.00
4B	12-20-24v	10	<b>£8.25</b>	85p
4C	12-20-24v	5	<b>£5.25</b>	65p
4D	3-12-18v	20	<b>£11.25</b>	£1.00
5A	3-12-18v	10	<b>£7.75</b>	85p
5B	3-12-18v	5	<b>£4.95</b>	65p
5C	3-12-18v	2	<b>£4.95</b>	65p
6A	48-56-60v	1	<b>£13.25</b>	£1.00
6B	48-56-60v	2	<b>£8.50</b>	85p
7A	6-12v	20	<b>£12.50</b>	£1.00
7B	6-12v	10	<b>£5.25</b>	65p
7C	6-12v	5	<b>£3.85</b>	60p
8A	17-32v	8	<b>£8.50</b>	85p
9A	12-24v	1	<b>£2.70</b>	50p
10A	9-15v	2	<b>£2.70</b>	50p
11A	8-0-8v	2	<b>£2.70</b>	50p

## 9 INCH FLYING LEADS ALL PRIMARIES 240V

Type No	Sec. Volt	Tap	Amperes
1	24-30-36	20	20
2	12-20-24	30	30
3	3-12-18	30	30
4	6-12	50	50

## CENTRE TAPPED L.T. TRANSFORMERS

Fully shrouded Terminal block connections Pri 220-240V. Screen Tapped sec 30-25-0-25-30v 2 amps **£4.95**, carr 60p 36-25-0-25-36v 5 amps **£9.95**, carr 85p 28-0-28v 10a **£12.50**, carr £1

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## STEP DOWN AUTO TRANSFORMERS

Open type Terminal block connections Tapped 0-25-35-45-55-65-75-85-95-240v 600 watts conservatively rated. Size 5½" x 4½" x 4½" **£4.75**. Carr 75p 300 watts **£3.00**. Carr 50p 200 watts **£2.00**. Carr 50p Gardners enclosed type auto transformers Tapped 0-110-115-210-230-250v conservatively rated 60 watts Totally enclosed **£2.00**. P.P 50p Partridge mains booster transformer Tapped 0-220-230-240-250v 500 watts open type terminal block connections **£3.00**. Carr 50p Drake isolation transformer PRI 200-220-240V. Sec 110v 50 watts. Open Type Terminal block connections **£2.75**. Carr 50p

Other Types Available: 80-1500 watts fully shrouded with American socket outlet and 6 ft mains lead. Let us know your requirements. Lists available

## GRESHAM MULTI-TAPPED L.T. TRANSFORMERS

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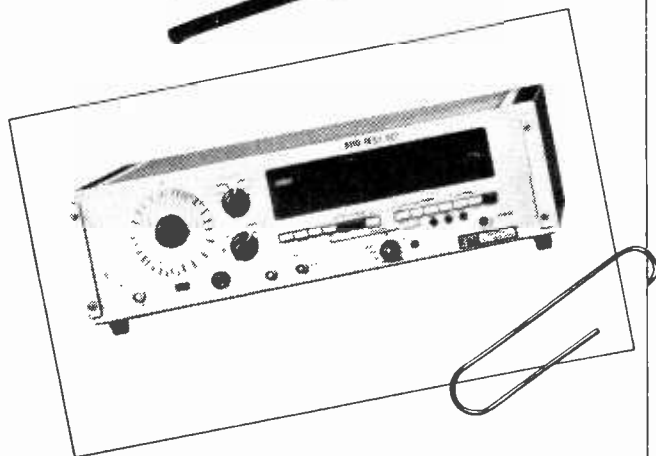
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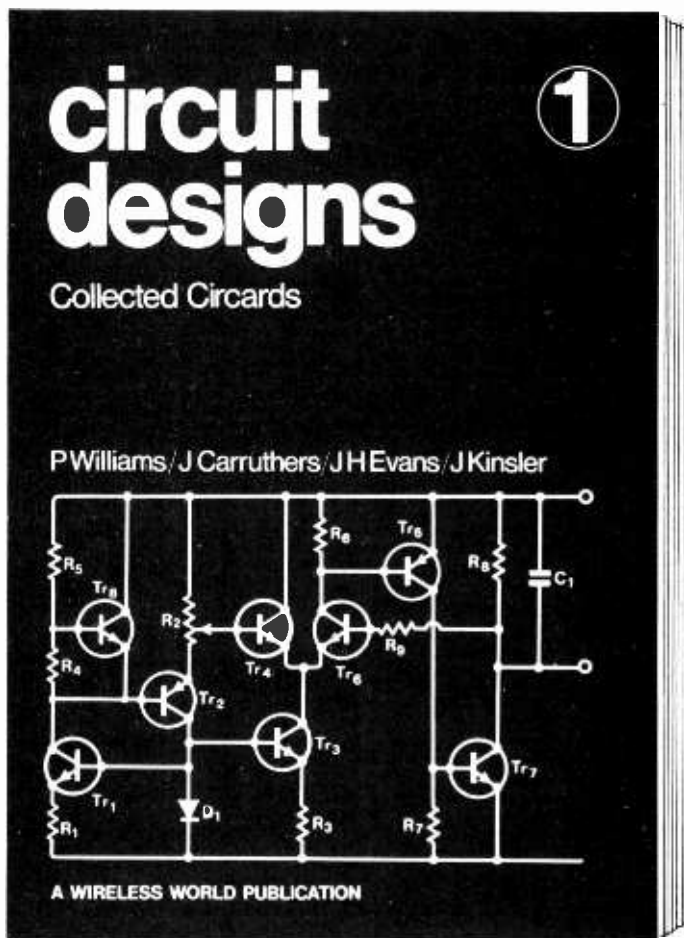
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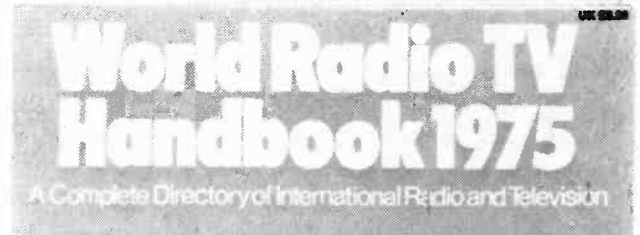
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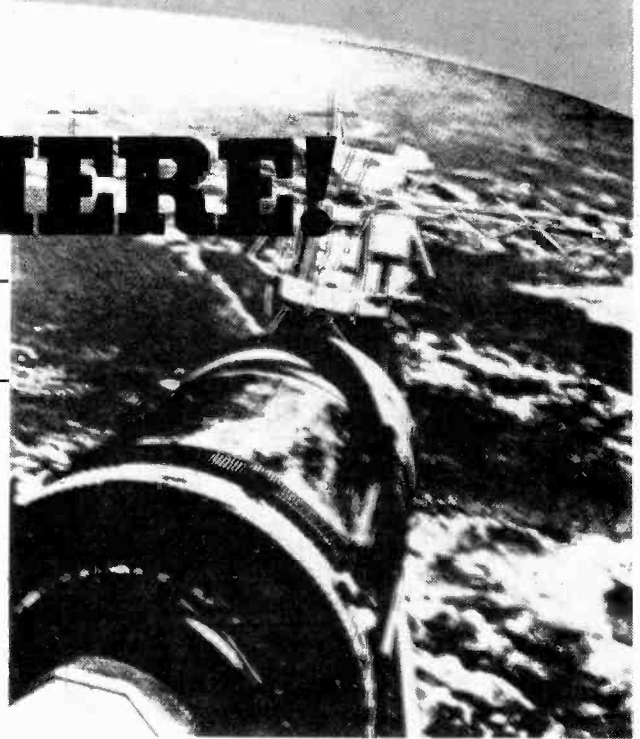
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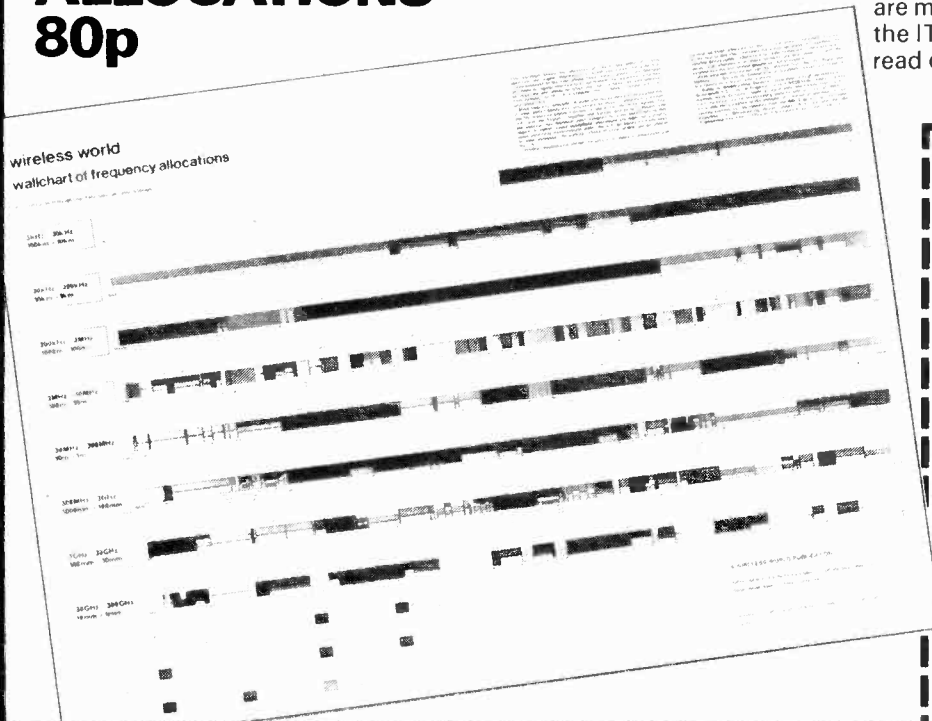
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To assist in the commissioning of prototype builds including systems testing, recording test results and diagnosing and correcting malfunctions of the equipment. Applicants should have at least two years experience in the test and commissioning of complex electronic equipment, and should be qualified to a minimum of ONC standard. Service within HM Forces will also be suitable.

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For full details and an Application Form, please return the coupon to Mr. D. D. Bennett, General Manager, Marconi Space & Defence Systems Limited, Hillend Industrial Estate, By Dunfermline, Fife.

Please send me details of career opportunities at Hillend.

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(4732)

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Now that Television has started in South Africa, OK Bazaars is all set to capture the major share of the market. We're the largest retail organisation in Southern Africa and are building up the most extensive and professional TV operation in the Republic. Because of the size of the Company's activities in this exciting new development we are able to offer outstanding prospects to experienced personnel, and in order to ensure first-rate service for our customers, we now need to enlarge our already substantial staff by appointing TV Technicians in various centres throughout the Country.

The work will entail carrying out repairs in the field and in the workshops, keeping records of time and materials involved and feeding back information to management on recurrent faults and defects in apparatus.

Essential requirements are a recognised apprenticeship or training course on radio and TV servicing and at least three years' experience in colour TV. Applicants should also possess a City & Guilds Final Certificate with RTEB colour endorsement or an equivalent qualification.

Salary will be at least £3750 per annum with an extensive range of fringe benefits including company assisted pension and medical aid schemes, full air passage, initial hotel accommodation and relocation allowances.

Interviews will be held in the UK, so write now with details of age, qualifications, experience to Mrs. M. Dunn (TVT), Austin Knight Limited, London W1A 1DS, including a telephone number where you can be contacted.

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(4755)



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Possession of one of these qualifies you for consideration for a Radio Officer post with composite signals organisation.

On satisfactory completion of a 7-month specialist training course, successful applicants are paid on a scale rising to £3,242 pa; commencing salary according to age — 25 years and over £2,383 pa. During training salary also by age, 25 and over £1,724 pa with free accommodation.

The future holds good opportunities for established status, service overseas and promotion.

Training courses commence at intervals throughout the year. Earliest possible application advised.

Applications only from British-born UK residents up to 35 years of age (40 years if exceptionally well qualified) will be considered.

Full details from:

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**Government Communications Headquarters**  
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**Cheltenham, Glos GL52 5AJ**  
**Telephone Cheltenham 21491 Ext 2270**

92

## CHELSEA COLLEGE UNIVERSITY OF LONDON ELECTRONICS TECHNICIAN GRADE 3

required as soon as possible for the Department of Pharmacy.

The work is concerned mainly with servicing a variety of instruments used within the department and some design and construction work is called for.

Applicants should hold appropriate qualifications at Intermediate Level and possess three years' experience, including training. Enthusiasm and initiative are important.

Salary £2,013-£2,343 plus £410 per annum London Allowance.

Application forms from Manager of Technical Services, Department of Pharmacy, Chelsea College, Manresa Road, London, S.W.3.

4752

# “We aim to match the best ten companies in the rewards and conditions we offer”

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What are the tangible results of this declared policy by Neville Cooper, STC Director with responsibility for personnel policies? What does it mean in terms of salaries and benefits, working conditions, prospects of promotion and development within the company? What does it leave unsaid about STC's attitude to its people and their needs as individuals?

STC – one of the world's leading companies in telecommunications and a pioneer of the new British Telephone Switching System, TXE4 – is looking for professional and technical engineers at all levels of experience for Advanced Systems Development, Application Engineering, Systems Design and Integration, and Circuit and Logic Design.

## STC – on record!

To answer some of the questions you might be expected to ask about us, Ken Corfield, STC's Managing Director, and three of his colleagues – Neville Cooper, Jock Marsh and Geoff Samson – have chosen to make a record, each explaining the thinking behind the tasks and challenges of his own specific area of responsibility, and outlining the opportunities within STC. In this way, you can build up a positive picture of the company as a whole: its attitudes, approach to business, present and long-term views.

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## Train to be an Electronics Technician

If you are 16-18 years old and would like a career in Electronics, our special 3 year training scheme provides the opportunity you are looking for.

We are offering you the opportunity to become an Electronics Technician in a fast expanding industry with an ever increasing demand for those with the ability to

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Our scheme includes well paid employment whilst training and day release to attend college to study for the City and Guilds Electronics Technician Certificate.

In addition to a practical interest in electronics you will require 'O' levels or CSE grades in

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Telephone or write to R. F. Honnor,

Personnel Manager,

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### UNIVERSITY OF GLASGOW

## ELECTRONIC RESEARCH ASSISTANT

Applications are invited for an Electronic Research Assistant in the Department of Physiology to join team working on electrical properties of nerve muscle and heart cells. No previous biological experience required. Applicants of degree standard may register for a postgraduate degree on a part-time basis.

Salary according to qualifications and experience in electronics within national salary structure for research staff (Range 1B £1809-£2757 or Range 1A £2118-£3990).

Applications to: Professor O. F. Hutter, Department of Physiology, University of Glasgow, G12 8QQ, from whom further particulars may be obtained.

In reply please quote Ref. No. 3681 FH.

4756

# Her Majesty's Government Communications Centre

HANSLOPE PARK,  
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has vacancies in the following fields of R & D work:

- (a) VHF/UHF COMMUNICATIONS
- (b) COMMUNICATION FIELD TRIALS
- (c) ACOUSTICS
- (d) MICROWAVES
- (e) GENERAL CIRCUIT DESIGN — ANALOGUE, DIGITAL
- (f) STATISTICS/OPERATIONAL ANALYSIS/SYSTEMS

### ANALYSIS

Most posts will be at Hanslope Park but some, in particular (f), will be in London. Posts in London carry a London allowance of £410 per annum in addition to the salaries quoted below.

Candidates for post (f) should be experienced scientists/engineers who have specialised later in one of the required fields. An ability to deal with non-technical people is essential.

Appointments will be made within the grades of Higher Scientific Officer except for (d) and (f) where appointments may also be made within the Senior Scientific Officer grade. The appointments will be established within Government Service with a non-contributory pension scheme.

### Higher Scientific Officer

Applicants should be under 30 years of age but this requirement may be waived if special qualifications or experience can be offered. They should have one of the following qualifications:

- (a) A degree in a scientific or engineering subject.
- (b) Degree-standard membership of a Professional Institution.
- (c) A Higher National Certificate or Higher National Diploma in a scientific or engineering subject
- (d) A qualification equivalent to (c) above

In addition the following relevant experience is required.

- (a) Applicants with 1st or 2nd class honours degrees -- at least two years' post-graduate experience.
- (b) Applicants with other qualifications -- at least five years' post qualifications experience.

Salary Scale £3254 - £4454 with entry point dependent upon experience beyond the minimum required

### Senior Scientific Officer

Applicants should be at least 25 and under 32 years of age, although the upper age limit may be waived if experience of special value can be offered.

Applicants should have obtained a 1st or 2nd class honours degree and have had a minimum of four years' appropriate post-graduate experience.

Salary Scale £4185-£5778 Entry will normally be at the minimum of the scale but applicants with experience of special value may be entered above the minimum

Applications, stating the field of work and the grade required should be made to

**Administration Officer**  
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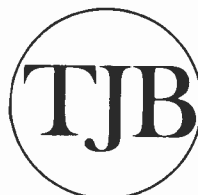
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If you are thinking of a change of career and would like to be involved in an undertaking which gives scope for personal development, and at the same time contributes to the wellbeing of the country, write in confidence, giving full details of your age, educational and technical qualifications and experience, and indicating the area of the country in which you would prefer to work, to:-

Mr. T. A. Lucas,  
Communications and Instrumentation Dept. (WW),  
British Gas, National Westminster House,  
326 High Holborn, London WC1V 7PT.



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4729

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We are looking for a man fully experienced in all aspects of this business with good product knowledge and capable of dealing at Government level on large contracts. He should be capable of working entirely on his own initiative and will report directly to the Managing Director.

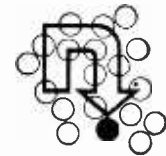
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(4758)



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to work in our audio group on the development of studio talkback and communications equipment used in TV studio broadcasting systems.

You should be 21-25, have HNC or equivalent plus 1-2 years' experience in the use and/or design of audio products.

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4745

**LINK**  
ELECTRONICS

Walworth Industrial Estate,  
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or

## Electronics Engineer

required by the Institute of Cancer Research at Sutton, Surrey, to join an active R and D programme on ultrasonic diagnosis of cancer. The work will be varied and responsible, in a joint hospital/research institute environment and will call for a range of practical abilities in the development and application of novel instrumentation. Previous experience in ultrasonics would be useful but is not essential.

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Applications with curriculum vitae in duplicate and naming two referees to: The Secretary, Institute of Cancer Research, 34 Sumner Place, London SW7 3NU, quoting ref. 300/G/85.

4742



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All the benefits of the world's largest radio-telephone exporters, could soon be yours. If you value your expertise highly, this is where to get most mileage from it.

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**Pye Telecommunications Ltd**

(4717)

Kensington and Chelsea and Westminster  
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Applicants with full details of career to date and quoting two referees, should be sent to Establishment Officer, The Middlesex Hospital, London W1N 8AA. Closing date for applications 2nd June, 1975.

4650

# RADIO ENGINEER

Telerenters (London & Provincial) Limited have vacancy for Senior Engineer at Watford.

The Engineer should have detailed knowledge of RF and audio measurements and be familiar with European specifications to enable him to implement and manage a test laboratory for the type approval of domestic radio, audio and recording equipment. Factory experience essential.

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### Pay

£2010 at 17, £2230 at 19, rising to £3385 a year.

### A Secure Future

with a non-contributory pension scheme, good prospects of promotion and a generous leave allowance. 5-day week of 42 hours.

### Interested?

Then telephone or write for an application form to: Mr J J Willis, Directorate of Radio Technology, Room 514, Waterloo Bridge House, Waterloo Road, London, SE1 8UA. Telephone 01-275 3006.

4722



*Home Office*

## SERVICE ENGINEER

Required to service our range of scientific and laboratory instruments, which include Fraction Collectors, U.V. Monitoring, Ultramicrotomy equipment. The applicant should be resident in an area North of the Thames to Luton or prepared to move. A good working knowledge of modern electronics and a scientific background is desirable.

The Company offers excellent working conditions including pension scheme, profit sharing bonus scheme, BUPA membership and Company car.

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AND

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Canada's Leader in Cable Television requires personnel for research and production departments.

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Opening for **CHIEF ENGINEER** — should have CATV or related experience. Electronics person strong in leadership, Methods and Mechanical Acumen required for capacity of **PRODUCTION MANAGER**.

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### CHELSEA COLLEGE UNIVERSITY OF LONDON

## ELECTRONICS TECHNICIAN

### GRADE 5

required for interesting design and development work in an Electronics Workshop, catering for the prototype requirements for teaching and research in the Departments of Electronics and Physics.

Salary £2,849-£3,305 per annum, including London Allowance.

Five-day, 37½-hour week.

Generous holidays.

Application forms and further details from Mr. M. E. Cane (5EW), Chelsea College, Pulton Place, London SW6 5PR.

4753

### CHELSEA COLLEGE UNIVERSITY OF LONDON ELECTRONICS ENGINEER

required to take charge of Electronics Workshop for the design and production of prototype electronic equipment for electronics and physics research and teaching, and also for the servicing and maintenance of a wide range of commercial electronic equipment.

A wide practical experience and a sound theoretical knowledge of electronics is essential. Experience in microwave instrumentation would be an advantage, five-day, 37½-hour week. Salary (Technical Staff Grade 6) £3,254-£3,860 per annum, including London Allowance.

Further details and application form from Mr. M. E. Cane (EW7), Chelsea College (University of London), Departments of Electronics and Physics, Pulton Place, Fulham, London SW6 5PR.

4754



**ELECTROSONIC LTD SE LONDON****SENIOR DEVELOPMENT ENGINEER****AUDIO PRODUCTS c£4200 pa**

Electrosonic Ltd are seeking a professional engineer with at least five years experience of developing audio equipment. He will primarily be required to make significant technical contributions to the company's new products which will range from AV replay equipment to studio mixers.

It is also expected that through his commercial awareness of the audio field he will help to define the product range and expansion in this important area of the company's business.

**MANAGER —****ELECTRONIC TEST DEPARTMENT c£3,500 pa**

A candidate is required having wide experience in a production test shop. Technical ability in analogue and digital circuitry is essential together with experience of supervising the work of others.

Duties will include the organisation and day-to-day running of the test shop, providing technical oversight, training of junior engineers, the introduction and programming of automatic test equipment and supervision of quality control.

**TEST AND SERVICE ENGINEERS****£2,400-£2,800 pa**

Vacancies exist in both these departments for electronic engineers having a minimum of two years experience of control and/or audio systems. On the job training will be given and opportunities for advancement are available. Service engineers will be required to work both in the factory and on site and the holding of a current driving licence is desirable.

The company is leader in the rapidly expanding fields of lighting control, audio and audio visual systems and offers a wide range of interesting work in an attractive environment and excellent conditions of employment.

Apply: Personnel Director, Electrosonic Ltd, 815 Woolwich Road, Charlton SE7 8LT.  
Tel: 01-855 1101



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We are looking for a first-class electro-mechanical service engineer to maintain television, film, electronic and other equipment including Shibaden 1212 colour cameras, IVC colour VTRs, Sony U-matic recorders, etc. This equipment is sited in our theatre, studio, cinema and boardrooms in Shell Centre and at our Conference Centre at Teddington.

The job also involves production of programmes, organisation of staff, design and building of prototypes of mechanical, optical and electronic units in our busy AV Centre.

Starting salary would be negotiable, dependent upon qualification/experience. 5 day week, contributory Pension Fund, free 3-course lunches, 4 weeks annual holiday. Sports and social facilities in the building, including squash, badminton, swimming.

Telephone or write for an application form to: Shell International Petroleum Company Limited, LP 112, Shell Centre, London SE1 7NA. 01-034 2828.

4767

### GLASGOW COLLEGE OF TECHNOLOGY PART-TIME B.Sc. DEGREE (C.N.A.A.) IN ELECTRICAL ENGINEERING with choices in Power or Electronic subjects

Holders of a good HNC or HND in Electrical/Electronic Engineering or related disciplines may be eligible to enter the above course commencing 18th August, 1975. If you are interested in the above course, write or telephone now for application form and further details to:

The Academic Registrar, Glasgow College of Technology, North Hanover Place, Glasgow, G4 0BA. (Telephone: 041-332 7090).

(4765)

### BRITISH MEDICAL ASSOCIATION DEPARTMENT OF AUDIO/VISUAL COMMUNICATION

## Electronics Officer

Up to £3008 (increase is currently being negotiated) + £410 London Weighting

With lively interest in Audio/Visual aids for education.

Duties will include liaising with medical teachers and providing information and advice on a wide range of equipment; supervising a workshop for repair and maintenance of closed circuit television and audio equipment for research purposes; supervising the design and construction of prototype equipment and an audio cassette duplication service; undertaking sound and television recordings in a small studio.

Applicants should have at least 5 years' experience in the educational uses of audio/visual aids.

Starting salary according to qualifications and experience.

Applications, with a full curriculum vitae and the names of two referees, to the Director, BMA House, Tavistock Square, London WC1H 9JP, not later than 11th July.

(4719)

THE ROYAL NATIONAL THROAT,  
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### PHYSICIST (BASIC GRADE)

Applications are invited for a newly established post of Physicist (Basic Grade) for work in the field of hearing disorders and the applications of hearing aids. Suitable candidates will have a degree in Physics and should have experience in electronics and acoustics. He/she will be based in a new electronic-acoustics laboratory and in the Hearing Aid Centre.

Salary scale £2046-£2562+ £312 London Weighting + current Threshold payments.

Applications giving details and names of two referees to Senior Administrative Assistant.

### ELECTRONICS TECHNICIAN

Grade 5

required for the Chemistry Department. Duties include the servicing and repair of a wide range of optical and electronic instrumentation, the design, construction and modification of electronic units concerned with instruments. Minimum qualification O.N.C. or equivalent. Salary on scale £2849 p.a.-£3305 p.a. (including London weighting) according to experience. Apply in writing giving full details to the Head Clerk (WW), University of London King's College, Strand WC2R 2LS.

4749

### CITY OF LONDON POLYTECHNIC TV ENGINEER

(MAINTENANCE) REQUIRED to join a small team working on the installation and maintenance of a wide range of equipment from CCTV equipment to slide projectors.

Applicants must have a sound practical knowledge of electronics and mechanics; relevant qualifications an advantage.

Salary Technician Grade 3 scale: £2,424-£2,754 including London Weighting. Entry point according to qualifications and experience.

Application forms and further details from The Assistant Secretary, City of London Polytechnic, 117/119 Houndsditch, London EC3A 7BU.

(4737)

### ELECTRONICS TECHNICIAN

(Grade 5)

required in the Department of Physiology to be responsible for the servicing of a wide range of sophisticated electronic instruments for both research and teaching and the design and construction of prototype apparatus. Good electronic background and qualifications essential. Some experience in medical or biological field preferable. Salary on scale £2849 per annum-£3305 per annum (including London weighting) according to age and qualifications, four weeks' annual holiday. Contributory Pension Scheme. Apply in writing with full details to the Head Clerk (WW), King's College, London, Strand WC2R 2LS.

4740

## TEST ENGINEERS

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(4764)

## VIDEO ENGINEER

Good all-rounder required by London's liveliest video dealers.

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In return we are prepared to pay a more than generous wage with fringe benefits.

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Peter Ellis, Technical Manager  
TELETAPE VIDEO  
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Telephone 743 1319 or 434 1267

(4757)

## UNIVERSITY OF SOUTHAMPTON

Research Fellow in  
Optical Communications

Applications are invited for a Research Fellow or Assistant to join an active group working on Optical Fibre Communications in the Department of Electronics. The work involves the use of fibres in multi-access communication systems including the development of couplers and junctions. The normal qualifications required are a PhD or equivalent research experience although applicants with other qualifications will be considered. Some knowledge of electronics, communications or opto-electronics is desirable. Salary will depend on experience and qualifications and will be within the range £1 809 to £3,813 (under review) plus Threshold payments.

Applications, including curriculum vitae and the names of two referees, should be sent to Mr. D. A. S. Copland, The University, Southampton SO9 5NH, quoting reference 383/R/WW.

(4744)

# Opportunities for Electronics Engineers

To change to wider fields of electronics  
— join the EMI Service Team at Hayes.

Vacancies exist on repair and calibration of a wide range of electronic test gear including oscilloscopes, DVMs, pulse generators, power supplies etc.

Also

Servicing and commissioning closed circuit television equipment including cameras, VTRs, Monitors etc.

Applicants should have at least 5 years practical experience.

These positions offer varied and interesting work. Attractive starting salaries, subsidised lunches, 4 weeks holiday and excellent sick pay and pension schemes.

For further details telephone or write to:- M. Ford, 01-573 3888, Ext. 2167, EMI Service, 254 Blyth Road, Hayes, Middlesex.



The international music, electronics and leisure Group.

4741

## Directorate of Radio Technology Telecommunications Officers

(£4,190-£4,620)

to be responsible for the study of radio propagation matters over the whole of the radio frequency spectrum (10kHz-275 GHz) and for the forward planning, management and regulation of frequency bands allocated to broadcasting, fixed, maritime and land mobile, and space services.

Duties also include: preparing specifications and type-approval of equipment for fixed and mobile services; application of computer techniques to frequency assignment problems; development of equipment for the location and suppression of radio interference; technical advice on all aspects of licensing of radio services and advice in connection with the international radio monitoring service.

Candidates (aged at least 25) must have ONC in Engineering (with a pass in Electrical Engineering 'A') or in Applied Physics or an equivalent qualification. In addition they must have had at least 7 years' experience of skilled work on radio, radar or other electronic work.

Salary, starting at £4,190, rises to £4,625. Good promotion prospects. Non-contributory pension scheme.

For further details and an application form (to be returned by 10 July, 1975) write to Civil Service Commission, Alencon Link, Basingstoke, Hants. RG21 1JB, or telephone Basingstoke (0256) 68551 (answering service operates outside office hours) or London 01-839 1992 (24 hour answering service). Please quote ref. T/9017.

HOME OFFICE, London

4720

## UNIVERSITY OF SURREY ELECTRONIC ENGINEER

Applications are invited for the above position in the Electronic Workshop of the Psychics Department. The person appointed will work, together with two other members of the technical staff, under the general direction of a Chief Technician.

Applicants should have a good electronics background, a sound theoretical knowledge and should have experience in the development and construction of computer interfacing and be familiar with nucleonic instrumentation. Qualification: HNC or equivalent. Salary scale: £2,844 - £3,450.

For further details and application forms please apply to the Staff Officer, University of Surrey, Guildford, Surrey GU2 5XH or Tel: Guildford 71281, Ext. 452.

(4654)

## NORTHAMPTON COLLEGE OF TECHNOLOGY

DEPARTMENT OF ENGINEERING

# Lecturer Grade I in Electrical Engineering

Applicants should have had previous experience of light current / electronic work and hold an H.N.C. or a final C.G.L.I. certificate with electronic subjects. Previous teaching is not essential, although desirable.

Duties will commence on 1st September 1975. Salary scale (under review) £1869-£3633 per annum plus threshold payment.

On 1st September 1975 the Northampton Colleges of Technology, Art and Education will amalgamate to form a new College of Higher Education (Nene College).

Further particulars and application forms can be obtained from the Chief Administrative Officer, Northampton College of Technology, St. George's Avenue, Northampton NN2 6JB. Telephone (0604) 713505.

4769

## PRODUCTION MANAGER

for small quartz crystal manufacturing plant

in

### NEW ZEALAND

An opportunity exists for a Production Manager familiar with all aspects of quartz crystal manufacturing for the communications market. Past experience should encompass grinding, vacuum plating and finishing to frequency. The company, Hatfield Crystals Ltd., has recently entered the field of quartz crystal filter manufacture thus, although not an essential, it would be useful if the applicant has knowledge of quartz crystal design, particularly monolithic crystal filters in the 10.7 MHz band.

The successful applicant must be prepared to reside permanently in New Zealand and will be sponsored through the Migration Department of the New Zealand High Commission. The company is located at Napier, North Island, in a temperate climate not unlike the South of France. An attractive salary together with the usual fringe benefits will be offered.

Applicants to write in the first instance to:

**The Managing Director  
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4646

# TEST ENGINEERS

We have vacancies for Test Engineers to fault find and test a wide variety of quality control equipment, with experience of working on chemical, gas and oil analysis essential.

These positions would be ideal for ex-service personnel with relevant experience.

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Ring Sylvia Borra 01-692 1271 Ext 393  
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**ELECTRONICS TECHNICIAN** required in Department of Psychology, University of Reading. Should have or be completing final C & G in Electronic Servicing or equivalent. Salary in scale £2439-£2895 p.a. (Grade 5). Apply with names of 2 referees and full details, quoting Ref. TZZ.23A to Assistant Bursar (Personnel), University of Reading, Whiteknights, Reading RG6 2AH. (4725)

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(4718)

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The duties will involve the servicing of our wide range of Video products, including recorders, cameras and microphones.

We are offering an attractive salary which will be based on qualifications and experience and generous staff discounts on all of our products.

**Please apply to: The Personnel Officer, Sony (UK) Ltd., Pyrene House, Sunbury-on-Thames, Middlesex. Tel: Sunbury 87644.**

4739

#### MINISTRY OF DEFENCE (ARMY DEPARTMENT)

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The post is open to men and women fully skilled and experienced in Television Servicing.

Appropriate ONC, C & G Certificate or equivalent qualification desirable. Selection is by test and interview.

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(4763)

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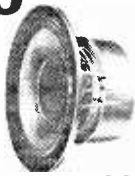
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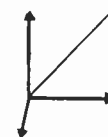
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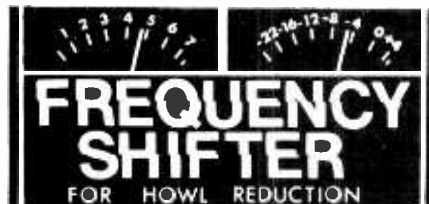
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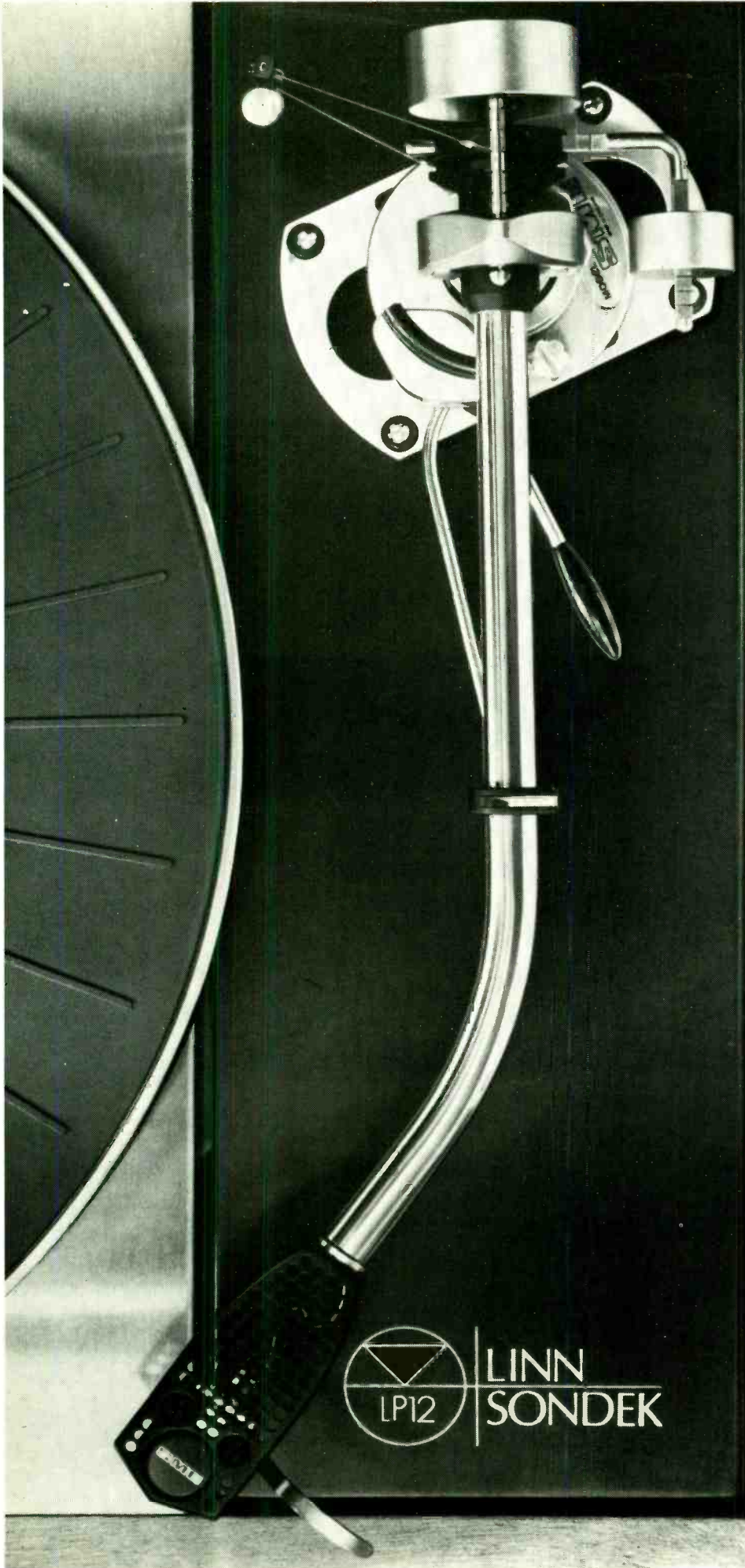
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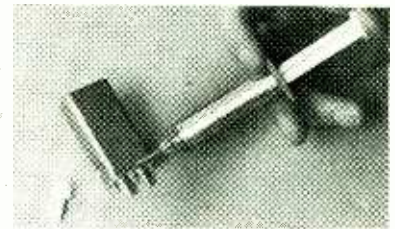
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