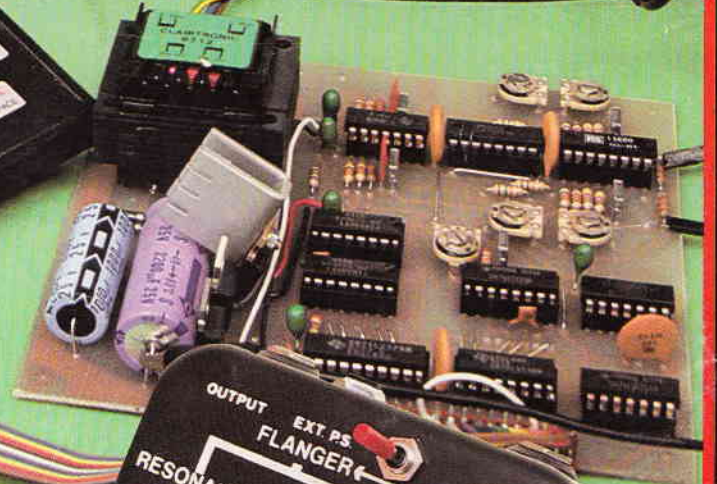


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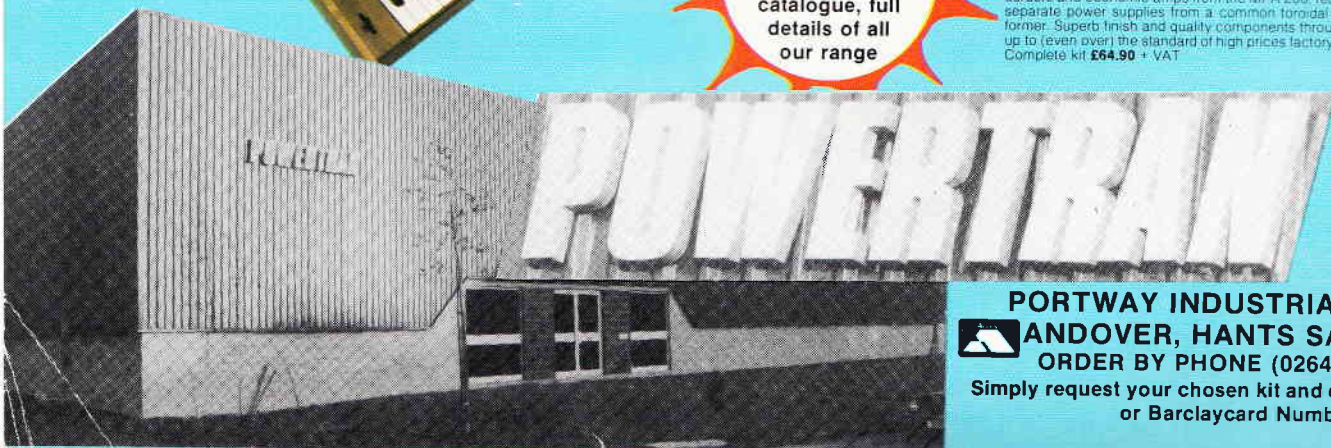
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- Due to lack of space, the fourth part of Bob Bennett's series on Machine Code Programming has been held over until next month.

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- EPROM PROGRAMMER REVISITED** 61
 A white flag flutters amidst the rubble of what was once 145 Charing Cross Road. The ETI staff, armed only with rolled-up assembler listings, have finally admitted defeat at the hands of the invading hordes. OK, we give in. Here it is, the complete listing, along with some further notes by Mike Bedford.



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THE-MINI-MYNAH

In our long-standing tradition of first-rate projects with third-rate puns for titles, here's our project for a speech synthesiser board. Its long list of features includes unlimited vocabulary from the use of allophone speech synthesis; four levels of inflection (we don't know of any other published design that allows inflection); 2K of on-board memory dedicated to speech generation, which allows the board to store 100 or more words; speech reproduction words, phrases or sentences stored in the memory selectable by a single command from the host computer; and simple interfacing requirements. So don't even think about building another design until you've seen ours!

BENCH PSU

One of the necessities of any experimenter's life is that of having to supply power for projects. Here is a supply that could be purpose built for electronics enthusiasts — in fact, it is purpose built by electronics enthusiasts! Output voltages are adjustable, but are nominally 5V at 2.5A and + and - 15V at 0.5A. And what's more, a full kit will be available, so start saving your pennies now!

MORE MEMORY FOR Z80 COMPUTERS

Following on from the project for a 6502/6800 64K DRAM board published in September 1983, we look at ways of increasing the available memory capacity of some common-or-garden Z80 computers. There are basically two methods — upgrading the existing memory, by substituting higher capacity DRAMs, and building a separate card with a block of memory on it. This article will look at the first, with the second method looked at in a future issue.



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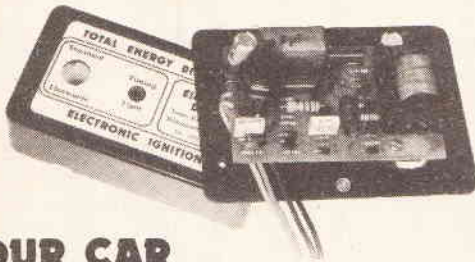
Articles described here are in an advanced state of preparation. However, circumstances may dictate changes to the final contents.

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DIGEST

New HP Research Centre In UK

At a press launch attended by the Secretary of State for Trade and Industry, Norman Tebbit, TV cameras and your very own editor, Hewlett Packard announced that they will be opening a new research laboratory in Bristol, to serve as their European Research centre. The company's main laboratories are in Palo Alto, California, and the new laboratory will be the company's first R&D establishment outside the USA.

The company will be commencing recruiting in the very near future, and the lab will be open in

the Spring of 1984 with around 50 research staff initially, rising to 200 by 1987.

According to HP's UK managing director, David Baldwin, the exact research objectives of the laboratory have yet to be decided, but will be in computing science. There will definitely be no semiconductor research.

David Baldwin and Norman Tebbit were very coy about the financial inducements that had been offered to make the company choose the UK (apparently, just about every country in the

world had also been under consideration). However, they denied that the prospect of government grants had been a major factor in the choice sufficiently often to make all the cynical journalists present convinced that it must have been.

However, the company's line was that the availability of well qualified graduates (despite the cut-backs in the technological universities such as Salford) and the excellence of the UK's universities (despite the cut-backs in technological universities such as Salford) were amongst the reasons — as was the apparent presence, on the M4 corridor, of the world's highest concentration of technical expertise.

Mr Baldwin stated that, with a few tax rule changes here and there, the establishment of the laboratory could lead to a large amount of money going to the UK universities in the form of research and equipment grants. HP currently spends around \$25m or more in this way in US Universities. The laboratory will also pro-

vide sufficient space for visiting researchers from Universities (and, presumably, Polys) to come and work on site.

HP reckon that for every project researched, there will be 50 other people employed by the company elsewhere, such as in production, marketing, etc, and therefore one could expect the research centre to generate around an additional 10,000 jobs given time. Obviously, there is absolutely no guarantee that these jobs will be generated in the UK, although according to a company representative, it would be more likely than if the lab had been sited in W. Germany.

One interesting feature is that although the first head of the laboratory will be an American, Donald L. Hammond who is currently head of the physical research centre at Palo Alto, one of his tasks will be to appoint a British successor. All those interested should join the editor in writing to Hewlett Packard Ltd, Nine Mile Ride, Wokingham, Berkshire RG11 3LL.

World's Thinnest Transformer

The latest transformer in the OB range from Avel-Lindberg stakes a claim as the thinnest yet, because, at 0.8VA, it is less than 10.5mm high (0.413in.) and will fit inside the smallest card frames. Dual primaries for 240 or 120V AC 50/60Hz mains operation are complemented by twin centre-tapped secondaries which give output voltages from 10V at 80mA to 48V at 17mA in series and 5 to 24V in parallel. These miniature transformers are proof-tested at 5kV a.c. and have a maximum operating temperature of

120°C (Class 2). They conform to IEC 65 Class 2, B.S.415 class 2 and VDE 0550 Class 2.

The normal method of fixing to a printed circuit board would be to direct solder the connecting pins, but where extra mechanical strength is required, the transformer can be screwed to the board using four holes moulded into the resin-filled, flat thermoplastic cases. The non-concentric twin primary and secondary windings are wound on separate bobbins which gives maximum isolation and low inter-winding capacitance. The secondaries can be series, parallel or independently wired, but if they are isolated from each other the applied potential between them must not exceed 500 V DC. The transformer is also short-circuit proof. Avel-Lindberg Limited, South Ockendon, Essex RM15 5TD, tel 070 885 3444.



Prize Tester

Fieldtech Heathrow are so convinced of the market potential of their LC53 Z-meter that they are running a free entry Autumn Sweepstake to promote the product with the Z-meter itself, valued at well over £550, as the prize. The unit is unique because it will dynamically test capacitors,

coils, SCR's and TRIAC's and, it is claimed, will find 75% of defective capacitors which value only meters will miss.

The LC53 tests capacitors for leakage current under full load with up to 600 volts applied, checks capacitor dielectric absorption, and has the capability to reform electrolytics. It will check for all coil defects in or out of circuit, and it automatically tests coils for effective Q using a US patent ringing test. It tests transmission lines for distance to open or short circuits within feet and it will also test dielectric strength to 600 volts.

For further details of the instrument and the sweepstake, contact Mike Dawson, Fieldtech Heathrow Limited, Huntavia House, 420 Bath Road, Longford, Middlesex UB7 0LL, tel 01-897 6446.

Plastic Shorts

Next time you investigate a defunct piece of electrical equipment and come across a resistor which appears to have gone short circuit, look again. That resistor may not be a resistor at all.

A system which is rapidly gaining acceptance within the electronics industry involves using wire links with plastic bodies to join tracks on printed circuit boards. The plastic body is usually

about the same size as that of a small resistor or diode and may, therefore, depending upon its colour, give rise to confusion in the minds of the unsuspecting.

The idea behind the use of these links is quite simple. PCB designers often need to link tracks on a board in circumstances which do not justify the use of a double sided board. The usual solution is to use wire links, but these have to be cut and inserted by hand, an expensive procedure especially where automatic insertion equipment is being used to mount the other components. Pre-formed plastic-bodied links

can be handled by the insertion equipment just as though they were conventional resistors, and even where boards are assembled by hand are quicker to insert than lengths of wire. The only restriction is that the pads on the PCB must be made the correct distance apart to accept the pre-formed leads, but since this already applies to just about every other component commonly used on PCBs there are no problems. Some companies use a number of standard lengths, eg 10, 15 and 20 mm, thus easing the task of the PCB designer.

In the past, companies have

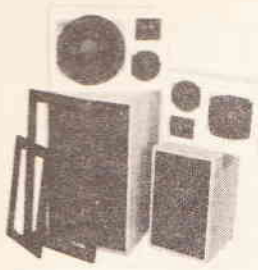
produced their own links or had them made to their own requirements. As the idea has caught on, however, a few companies have entered the market with pre-formed links. One of these is Nortronic, who call their products Zerohm Resistors. They are indeed about the size of a small resistor and have a brown body with yellow banding. Nortronic claim that they are chip resistant and have British Telecom approval. Nortronic Associates Limited, Gateway, Drew Industrial Estate, Crewe, Cheshire CW1 1YY, tel 0270 586161.



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Price £14.90 each + £2.00 P & P.
 5" 30W system - recommended cabinet size 160 x 175 x 295mm
Price £13.90 each + £1.50 P & P.

Designer approved flat pack cabinet kits, including grill fabric. Can be finished with iron on veneer or self adhesive vinyl etc.
 8" system cabinet kit **£9.00 each + £2.50 P & P.**
 5" system cabinet kit **£7.00 each + £2.00 P & P.**



STEREO CASSETTE TAPE DECK MODULE

Comprising of a top panel and tape mechanism coupled to a record/play back printed board assembly. Supplied as one complete unit for horizontal installation into cabinet or console of own choice. These units are brand new, ready built and tested.

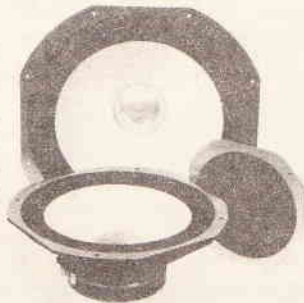
Features: Three digit tape counter. Autostop. Six piano type keys, record, rewind, fast forward, play, stop and eject. Automatic record level control. Main inputs plus secondary inputs for stereo microphones. **Input Sensitivity:** 100mV to 2V. **Input Impedance:** 68K. **Output level:** 400mV to both left and right hand channels. **Output Impedance:** 10K. **Signal to noise ratio:** 45dB. **Wow and flutter:** 0.1%. **Power Supply requirements:** 18V DC at 300mA. **Connections:** The left and right hand stereo inputs and outputs are via individual screened leads, all terminated with phono plugs (phono sockets provided). **Dimensions:** Top panel 5 3/4 x 11 1/2 in. Clearance required under top panel 2 1/4 in. Supplied complete with circuit diagram and connecting diagram. Attractive black and silver finish.
Price £26.70 + £2.50 postage and packing.
 Supplementary parts for 18V D.C. power supply (transformer, bridge rectifier and smoothing capacitor) **£3.50**



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THREE QUALITY POWER LOUD-SPEAKERS (15", 12" and 8" See Photo). **Ideal for both Hi-Fi and Disco applications.** All units have attractive cast aluminium (ground finish) fixing escutcheons. **Specification and Prices.**

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12" 100 watt R.M.S. Impedance 8 ohms. 50 oz magnet 2" aluminium voice coil. Res. Freq. 25Hz. Freq. Resp. to 4 KHz. Sens. 95dB. Price: £24.50 each + £3.00 P&P
8" 50 watt R.M.S. Impedance 8 ohms. 20 oz magnet. 1 1/2" aluminium voice coil. Res. Freq. 40Hz. Freq. Resp. to 6 KHz. Sens. 92dB. Black Cone. Price: £9.50 each. Also available with black protective grille Price: £9.99 each. P&P £1.50.



12" 85 watt R.M.S. MCKENZIE C1285GP (LEAD GUITAR, KEYBOARD, DISCO) 2" aluminium voice coil, aluminium centre dome, 8 ohm imp., Res. Freq. 45Hz., Freq. Resp. to 6.5KHz., Sens. 98dB. Price: £23.00 + £3 carriage.
12" 85 watt R.M.S. MCKENZIE C1285TC (P.A., DISCO) 2" aluminium voice coil. Twin cone. 8 ohm imp., Res. Freq. 45Hz., Freq. Resp. to 14KHz. Price £23 + £3 carriage.
15" 150 watt R.M.S. MCKENZIE C15 (BASS GUITAR, P.A.) 3" aluminium voice coil. Die cast chassis, 8 ohm imp., Res. Freq. 40Hz., Freq. Resp. to 4KHz. Price: £47 + £4 carriage.

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TYPE 'A' (KSN2036A) 3" round with protective wire mesh, ideal for bookshelf and medium sized Hi-fi speakers. **Price £4.29 each.**

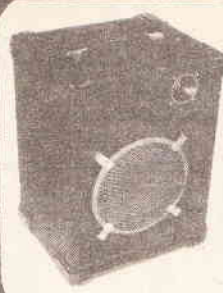
TYPE 'B' (KSN1005A) 3 1/2" super horn. For general purpose speakers, disco and P.A. systems etc. **Price £4.99 each.**

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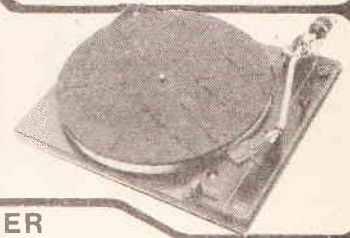


3 watt FM Transmitter

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Price £31.35 each. £2.50 P&P



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NEW OMP100 Mk.II POWER AMPLIFIER MODULE Power Amplifier Module complete with integral heat sink, toroidal transformer power supply and glass fibre p.c.b. assembly. Incorporates drive circuit to power a compatible LED Vu meter. New improved specification makes this amplifier ideal for P.A., Instrumental and Hi-Fi applications.

SPECIFICATION
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Loads:— Open and short circuit proof 4/16 ohms.
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S.N.R. (Unweighted):— -118dB ±3.5dB
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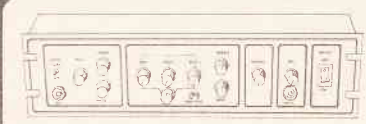
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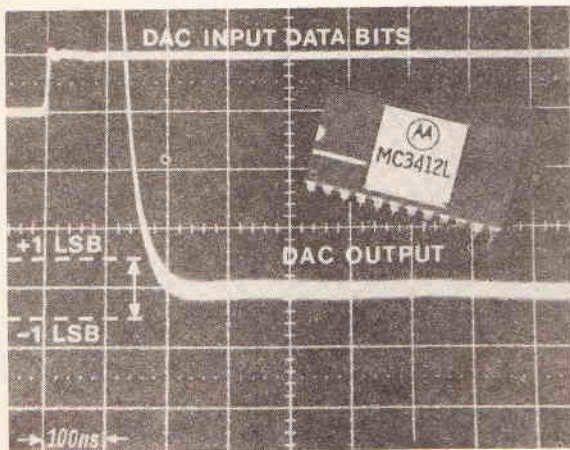
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High-Speed 12-bit D to A

Motorola has introduced a high-speed 12-bit digital to analog converter, the MC3412/3512, which uses monolithic bipolar and thin film resistor technology to provide high stability and fast settling time, and which is designed to work with a minimum of external components.

Active laser trimming of thin film resistors at wafer level gives guaranteed limits of gain and offset errors of $\pm 0.25\%$ FSR (full scale range) and $\pm 0.05\%$ FSR respectively without external adjustment. Monotonicity is guaranteed over the full temperature range and an innovative bit switching scheme ensures that settling time will be no greater than 400 ns

to $\pm 1/2$ LSB.

The converter includes an internal precision 10 volt bandgap reference and span/bipolar offset resistors. With the addition of one external op-amp, the precision span and bipolar offset resistors provide calibrated unipolar or bipolar full scale output voltage ranges of 0 to 5.0, 0 to 10, ± 2.5 , ± 5.0 and ± 10 volts. A CMOS/TTL threshold control pin permits selection of either CMOS or TTL logic levels at the data inputs.

Packaged in a 24-pin ceramic DIP, the MC3412/2512 is pin-compatible with the popular AD563 and AD565 digital to analog converters, and is available in commercial and military temperature ranges. For further information contact Motorola Ltd., European Literature Centre, 88 Tanners Drive, Blakelands, Milton Keynes MK14 5BP, tel 01-352 0041 ext 34.

Single Chip Data Acquisition Controller

All the functions required for intelligent data acquisition and signal monitoring are contained in the CY600 Analog/ASCII Data Acquisition Controller which is being introduced by Weyfringe. The chip is designed to be placed between A/D converters and an 8-bit host computer system.

When programmed, each CY600 channel will scan one or more A/D signals and inform the host when specified conditions are met, freeing the host system from signal monitoring tasks. The minimum CY600 contains two channel buffers which can be programmed with the instructions and conditions to be monitored. Each channel is assigned six registers to hold user defined con-

stants, A/D readings, or the results of arithmetic computations. Each channel can monitor its own signals or access any other channel's registers (cross channel correlation) so the device can test for several conditions by using different instructions in each channel. The maximum version of the CY600 is given up to four channels with larger program buffers and eleven registers per channel by adding an 8156 memory and I/O expansion chip.

The CY600 commands control the A/D converters, select channels and register and perform arithmetic operations (+, -, /) and conditional tests (<, =, >). Expressions combining all of the above provide comparisons of the signals and registers so that if a specified condition arises, the CY600 interrupts the host, and the host may then query the CY600 to determine the cause of the interrupt. For further information contact Mr Harry Gleghorn, Weyfringe Limited, Longbeck Road, Marske, Redcar, Cleveland TS11 6HQ, tel 0642 470121.

32K Byte DRAM

Mostek Corporation have introduced a 256K DRAM which they claim is the first on the market with 32K x 8 organisation. The MK4856 is produced using scaled NMOS technology which allows access times down to 100 ns. The address system is not multiplexed and Mostek say that this will eliminate the need for system logic and thus simplify timing. The device also has an integral refresh counter, further reducing external logic count. The 28 pin DIP version has the standard pinout and is available in plastic (N suffix) or ceramic (P suffix) form and a leadless chip carrier version (E suffix) is also available. The MK4856 is available with access times of 100 ns, 120 ns, or 150 ns and further information can be obtained from Mostek UK Ltd, 1 Valley Drive, Kingsbury Road, London NW9, tel 01-204 9322.

Microwave Amplifiers

NEC have introduced two new ICs which are claimed to offer a constant 16 dB gain from DC to 1.2 GHz. The MM765 and MM766 have built in temperature compensation to ensure stable bias and have an input and output impedance of 50 ohm, allowing devices to be cascaded where higher levels of gain are required. The MM765 operates at 10V and can be supplied in 8-pin or TO-33 packages, while the MM766 operates at 5V and is available in DISK-mold, 8-pin MINI, 8-pin DIP, and TO-72 packages.

Also new from NEC are a series of silicon NPN epitaxial transistors which offer up to 9 dB of gain at 1 GHz and have a noise degradation figure of 1.1 dB. The NE-856 series have a high current capability and come in four package styles including TO-92 and SOT-23. NEC Electronics UK Ltd, 116 Stevenson Street, New Stevenson, Motherwell ML1 4LT, tel 0698 732221.



Dot-Matrix Displays

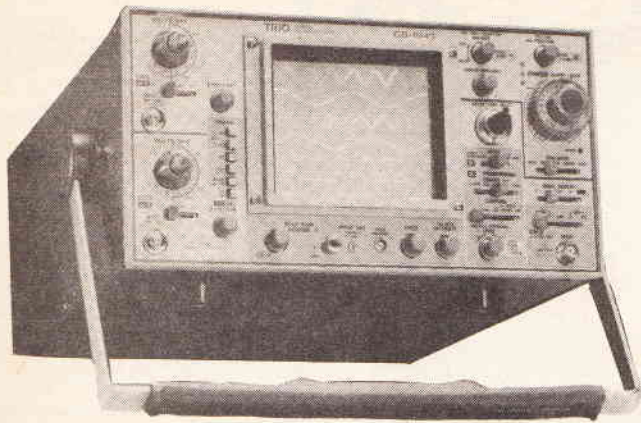
Nineteen new models of planar gas discharge (PGD) flat-panel, dot-matrix display subsystems have been introduced by Beckman Instruments. The displays, which complement the current one-line Beckman displays, enable large amounts of information to be presented where space is limited.

DC planar gas display technology produces high visibility yellow-orange light emission on a high-contrast black background. The height of the light emitting area is from 0.24 to 3.7 in and the width from 4.8 to 8.7 in. The full-controller versions interface using a standard 8-bit parallel micro-processor data bus. The alpha-

numeric units provide drivers, refresh RAM, a character generator and editing features, depending on model, allowing the user to display 5 x 7 dot matrix characters. The graphic units do not contain a character generator but allow each dot to be individually addressed so that characters and graphic patterns can be created with unlimited flexibility.

The driver-only versions provide cathode and anode drivers, the user having to supply external scanning and drive signals and design the controller with a data interface, character generator and refresh RAM.

The panels, fully guaranteed by Beckman for one year, are available in the UK from Beckman Instruments Ltd, Milen House, 11 Wagon Lane, Sheldon, Birmingham B26 3DU, tel 021-742 7921.



Dual Timebase 'Scopes

Trio have introduced a range of dual timebase oscilloscopes which are claimed to represent the ultimate in modern 'scope technology with regard to functions available, specification, reliability and value for money.

The CS-1040 and CS-1060 are three channel, six trace 'scopes with bandwidths of 40 MHz and 60 MHz respectively. Both use a large rectangular domed mesh,

post-accelerator CRT with 12 KV and 16 KV of accelerator potential, providing both high intensity and excellent resolution. Their inner face graticule eliminates parallax errors, while the auto focus maintains a sharp clear wave-form display at all times. Vertical axis sensitivity is continuously adjustable from 1mV/cm through 5V/cm, the very sensitive 1mV/cm range being of great assistance in observing complex, low level waveforms. Part of the input signal is diverted and fed to an output at approximately 50mV/cm of the input

level, the gain making it easy to measure frequency using normal frequency counters.

Alternate delayed sweep provides magnification of an intensified portion of the waveform simultaneously with the original. Channels 1, 2 and 3 can be displayed together using the main sweep, with the individual delayed waveforms of these channels simultaneously shown using the alternate sweep function to give a 6 trace capability. Sweep time is continuously variable from 0.5 sec/cm to 5 nanosec/cm with an internal delay line to provide accurate observation and measurement of the leading edge of high frequency signals. A $\pm 3\%$ accuracy allows for extremely precise waveform measurement.

Video signals both vertical and horizontal can be observed using a new video clamping function in which manual syncing has been eliminated, ensuring high stability syncing. Other features include V mode triggering, quickly switchable alternate and chop, high sensitivity X-Y mode, auto-free run, trace rotation, trigger holdoff, single sweep, line and auto sync, sweep and gate output, add and subtract, vertical control of delayed waveforms, and intensity modulation.

Completing the range is the CS-2110 four channel, eight trace 100 MHz oscilloscope. Sensitivity over its normal bandwidth is 1mV/cm and it will trigger to beyond 140 MHz. The CS-2110 has an inner face graticule, and an accelerator potential of 20 kV ensures that the display remains bright and sharp even when viewing high speed signals on the 2 ns/cm sweep range. In addition to the features found on the other two models, the CS-2110 has an accuracy of $\pm 2\%$, a channel-to-channel skew time of less than 500 ps, and completely independent A and B sweeps.

All three models come with a two year guarantee and a full range of accessories is available. The CS-1040 and CS-1060 cost £638.00 and £799.00 respectively, exclusive of packing, delivery and VAT, and are available from House of Instruments, Clifton Chambers, 62 High Street, Saffron Walden, Essex CB10 1EE, tel 0799 24922, or from Dawne Instruments & Electronics, Shields Road, Bill Quay, Gateshead NE10 0RS, tel 0632 695117. The CS-2110 costs £1399.00 exclusive of packing, delivery and VAT and is available from House of Instruments at the address above.

Computer Filter Plug

Galatrek International Ltd have introduced a new Filter Plug which can be fitted to the supply cable in place of a standard 13 amp plug and will protect micro and minicomputers, word processors and all voltage sensitive equipment from mains born interference.

This compact unit will protect equipment from transients and spikes which can wipe out memory and corrupt data. It also

provides protection against momentary supply interruption, mains RF interference and lightning disturbance. The current rating of 2 amps is sufficient for most micros and accessories, and frequency is 50/60 Hz. The Filter Plug is available as described, or in a small box with a socket outlet to choice for any country in the world and a flylead mains input, for £29.95 including VAT and post and packing. Order from the manufacturers, Galatrek International Ltd., Scotland Street, Llanrwst, Gwynedd, North Wales, tel 0492 640311.

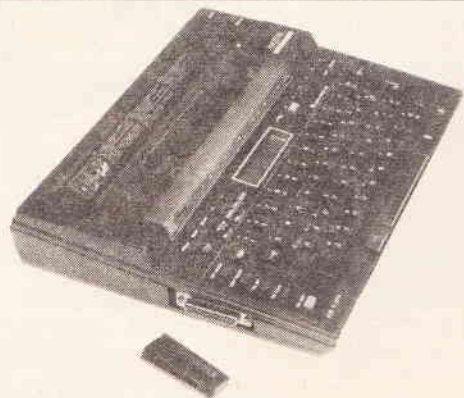
Low Cost EPROM Eraser

Ground Control have introduced a low cost ultra violet EPROM eraser which is aimed at development laboratories, home computer enthusiasts, and other applications where rapid erasure of just a few EPROMs is required.

The Uvipac EPROM Eraser is mains powered and will erase up to three EPROMs of any size at one time, or one CPU with on-board EPROM. Erasure takes between five and twenty minutes depending upon the type of EPROM and the Uvipac can be supplied with a built in fifteen

minute timer if required. EPROMs are simply loaded into the conductive foam pad supplied and inserted into the unit. When the door has been closed and the unit switched on, an optical fibre indicator shows that the eraser is operating. The complete unit measures just 90 x 80 x 49 mm and spare conductive foam pads and UV tubes are available from the manufacturers.

The basic Uvipac eraser costs £19.95 and the Uvipac-T with built-in timer costs £24.95. Both prices include VAT, and postage and packing for the UK is £1.50. Ground Control, Alfreda Avenue, Hullbridge, Essex SS5 6LT, tel 0702 230324.



Baby Brother

Brother's new EP-22 is probably the smallest and lightest typewriter in the world, and its plain paper thermal printing system makes it one of the quietest as well. It is battery powered, fully portable, and has a built-in RS-232C interface which allows it to be used as a printer with personal computers.

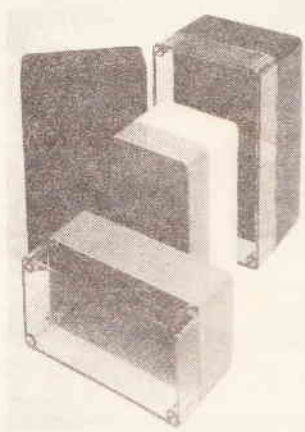
The EP-22 is no bigger than an A4 pad and its weight, including batteries, is just 5 lbs. The 5 x 7 dot matrix printer can be used with either thermal paper or with plain paper by means of a cassette-loading thermal ribbon. The calculator style QWERTY keyboard features a second shift for all the accents used in Roman script European lan-

guages, a range of signs for arithmetic and chemical formulae, and automatic superior or inferior numerals. A sixteen character LCD with adjustable angle brightness allows text to be checked, and if necessary amended using the 32 character correction buffer. Up to a page of corrected text can be stored in the 2K memory, ready to be printed at the touch of a button, and the display indicates the amount of memory remaining. The EP-22 can also be used as a 12 digit calculator.

The EP-22 comes complete with batteries, 3 thermal cassette ribbons, and both thermal and plain paper, and costs £169.95. Jones & Brother, Office Equipment Division, Shepley Street, Audenshaw, Manchester M34 5JD, tel 061-330 6531.

Now You See It...

Boss Industrial Mouldings Ltd have introduced a series of coloured tops to complete their range of ABS BIM 2000 Bimboxes. The existing range is available in seven sizes ranging from 100 x 50 x 25 mm to 190 x 110 x 60 mm and features a choice of five different coloured bases with a clear top. The new tops are made from the same material and come in the same five colours as the bases, allowing you to select matching or contrasting case sections as desired. Colours available are black, grey, white, orange and blue and all cases incorporate slots on a 0.2" spacing which can support PCBs. The case parts are secured by screws inserted through the base



and when assembled have excellent water repellent properties. Boss Industrial Mouldings Ltd, James Carter Road, Mildenhall, Suffolk IP28 7DE, tel 0638 716101.

Touch Sensitive Keyboard

The Concept keyboard has a flat surface which is divided into an 8 x 16 matrix of touch sensitive areas, each producing a unique 7-bit ASCII code which the programmer defines as required. The surface accepts A4 size overlay sheets which can be marked as desired to define areas and functions, and the manufacturers claim that it will work with any microcomputer.

The keyboard is intended for educational use, allowing pupils to communicate with a computer using a minimum of clearly marked functions rather than hav-

ing to cope with the complexity of a full QWERTY keyboard. Other possible applications include games, demonstrations, and simulation exercises. The format obviously lends itself to the representation of, for example, a floor plan around which people and furniture must be moved. It is possible to use a number of areas together and thus produce large touch sensitive pads which could be used by those who have handicaps or are otherwise unable to manipulate a conventional keyboard.

The Concept keyboard comes complete with full documentation, a connecting lead to suit the majority of microcomputers, and a set of demonstration software. Star Microterminals Ltd, 22 Hyde Street, Winchester, Hampshire SO23 7DR, tel 0962 51422.

SHORTS

● Downing Electronics have introduced a portable test pattern generator for use with all 525 and 625 line RGB display units. It provides 9 different patterns, has a signal frequency accuracy of $\pm 0.02\%$, and will test both separately synchronised and green signal pulse synchronised units. Cost is £325.00 plus VAT from Downing Electronics Ltd, 24 Downing Road, Reading, Berkshire RG3 5BB, tel 0734 22556.

● An international users group for owners of Oric-1 microcomputers has recently been set up. The Oric Owner's/Users Group (International) Ltd has the full approval of the computers' manufacturers and produces a monthly magazine called Oric Computing. Membership costs £10 a year, and £1 plus an A4 SAE will bring you full details and a sample magazine. 1 Marlborough Drive, Worle, Avon BS22 0DQ, tel 0934 510279.

● The NMS Relay Controller is designed for use with the ZX Spectrum and has four channels each with a double pole 5A 240V relay. The relays are operated by simple BEEP commands either from a program or the keyboard, and the unit plugs into the MIC socket leaving the expansion port free. It costs £24.95 plus £1.50 post and packing from Ness Micro Systems, 100 Drakies Avenue, Inverness IV2 3SD, tel 221 194.

● Cricklewood's latest catalogue covers 31 sides of A5 with mail order electronics parts, many of them illustrated. Items listed include semiconductors, books, tools, connectors, cases, switches, etc and copies cost £1 including postage from Cricklewood Electronics Ltd, 400 Cricklewood Broadway, London NW2 3ET, tel 01-452 0161.

● Bulgin have produced new catalogue listing their range of bulkhead mounting and integral IEC socket type mains filters. Ratings up to 6A are covered. Also new is a catalogue describing their Buccaneer range of waterproof connectors covering both mains and signal applications. A.F. Bulgin & Company PLC, Bypass Road, Barking, Essex IG11 0AZ, tel 01-594 5588.

● Inmac have produced an 88 page illustrated catalogue of computer and business accessories. Their range includes dedicated accessories for Apple and CBM machines and general accessories like cables, disc systems, etc to suit most other machines. The catalogue is free from Inmac UK Ltd, Davy Road, Astmoor, Runcorn, Cheshire WA7 1PZ, tel 09285 67551.

● Riscomp's US 5063 is an ultrasonic movement detection module which processes the received signal using digital techniques. It offers a choice of three levels of discrimination, fixed alarm time, exit delay, and selectable entrance delay and costs £13.95 plus VAT. Riscomp Ltd, 21 Duke Street, Princes Risborough, Bucks HP17 0AT, tel 08444 6326

● Salford University are running a series of one, two and three day short courses during December and January on the BBC, Apple II and CBM microcomputers. The courses cover all levels from complete beginner upwards and each student is guaranteed individual use of an appropriate machine. Details from The Microprocessor Short Courses Unit, Department of Electronics & Electrical Engineering, University of Salford, Salford M5 4WT, tel 061-736 4843 ext 248.

● The Integrex BX80 7—colour printer is designed for use with the BBC microcomputer and will work in all modes, including mode 7 Teletext, using the supplied colour screen dump listing. It prints at 125 cps on plain paper, has an internal 2.5K byte buffer, and connects to the BBCs RS-423 socket using the lead supplied. Price is £495 plus VAT from Integrex Ltd, Portwood Industrial Estate, Church Gresley, Burton-on-Trent, Staffs DE11 9PT, tel 0283 215432.

● Further to last month's report of a record number of bankruptcies among British electronics companies, a recent surprise casualty is Scopex Instruments Ltd. It may be of some consolation to owners of Scopex products to learn that a former design engineer with the company has formed a new company, Mendascope, which offers a full repair service including collection and free estimate. Mendascope Ltd, Otter House, Western Underwood, Olney, Bucks MK46 5JS, tel 0234 712445.

● Make light work of different number base arithmetic with Casio's new FX450. This solar-powered scientific calculator will rapidly convert between binary, octal, decimal and hexadecimal, has 64 functions and holds eight fundamental constants in memory. It comes in a protective folding wallet and costs £22.95. Casio Electronics Co. Ltd, Unit 6, 1000 North Circular Road, London NW2 7JD, tel 01-450 9131.

● Wilmslow Audio's new catalogue doesn't just list loudspeakers by manufacturers like Tannoy, Kef, Gauss and Chartwell, it also contains kits, amplifiers, microphones and stands, effects units, and a lot of useful information. Price is £1.50 from Wilmslow Audio Ltd, 25/39 Church Street, Wilmslow, Cheshire SK9 1AS, tel 0625 529599.

● The AMS 3" disc drive which is suitable for use with the BBC microcomputer is to be sold through W.H. Smiths. The unit comes in 100K format at £225 or 200K format at £399 and runs from the BBCs power supply. A number of software houses have produced packages for the drives.

● The 1984 London Home Computer Show runs from Friday January 6th to Sunday 8th in the large New Hall of the Royal Horticultural Society, just around the corner from the Old Hall where it was staged last year. The show is aimed at microcomputer hardware and software enthusiasts and is open from 10 am to 6 pm each day (4 pm Sunday). Admission costs £2.00 or £1.50 if you're under sixteen.

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VECTOR GRAPHICS

4,294,967,296 vectors should take over a year to draw, even at 100 per second. However if you want to try — the ETI Graf-vec will do it.

This project takes us away from the familiar world of the TV display and shows us instead the other principal means of producing a picture. The ordinary TV set produces a picture by moving an electron beam backwards and forwards across a phosphor coated screen so that it traces a fixed number of parallel horizontal lines. The actual picture is produced by turning the beam on to display a bright dot at the right time and turning it off where no light is required. This method works very well for broadcast pictures but is sometimes not so good for pictures generated electronically. For a home computer to generate a picture, it must generate a pattern of bits which determine when the electron beam in the display tube is to be on and off. Since the transitions can only occur at discrete time intervals, the picture produced does not

always appear as smooth as we might wish. This effect is usually most noticeable on diagonal lines where there are marked contrast changes.

While we cannot pretend that this project will replace a TV type of display for home computer applications, it does provide an interesting alternative output device for graphics.

The method employed by the Graf-vec in producing a picture is to define the start and finish of a line and cause an electron beam to traverse the intervening space relatively slowly. Drawing many such lines in a short space of time allows us to build up a picture. The main disadvantage of this method is that if too many lines are drawn the whole display will appear to flicker. This can be reduced by the use of long persistence phosphors if available.

As described, the Graf-vec will

draw lines between any two points on a 256x256 grid. The relatively simple circuitry used does not compensate for differing line lengths changing the brightness but still gives an interesting result.

The Circuit

The circuit consists of a power supply, digital input and control section, and two linear scan generators. The basic mode of operation requires a data source — probably your trusty home computer — to put two bytes of data into the device to represent the coordinates to which a vector is to be drawn (The starting point is assumed to be where you are now). The Graf-vec will draw the vector and then wait for the next set of data and indicate that it is ready. The digital input circuitry of the Graf-vec is designed so that one byte of the next vector can be input at any time as it is stored in a

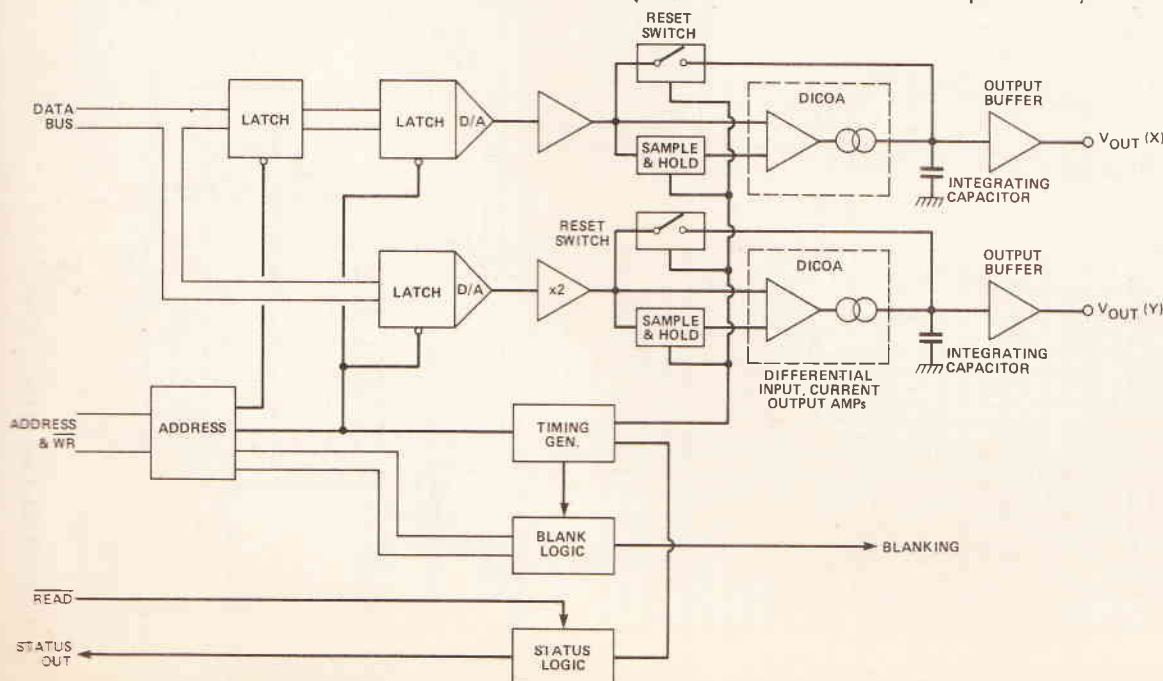


Fig. 1 Block diagram of the Graf-vec.

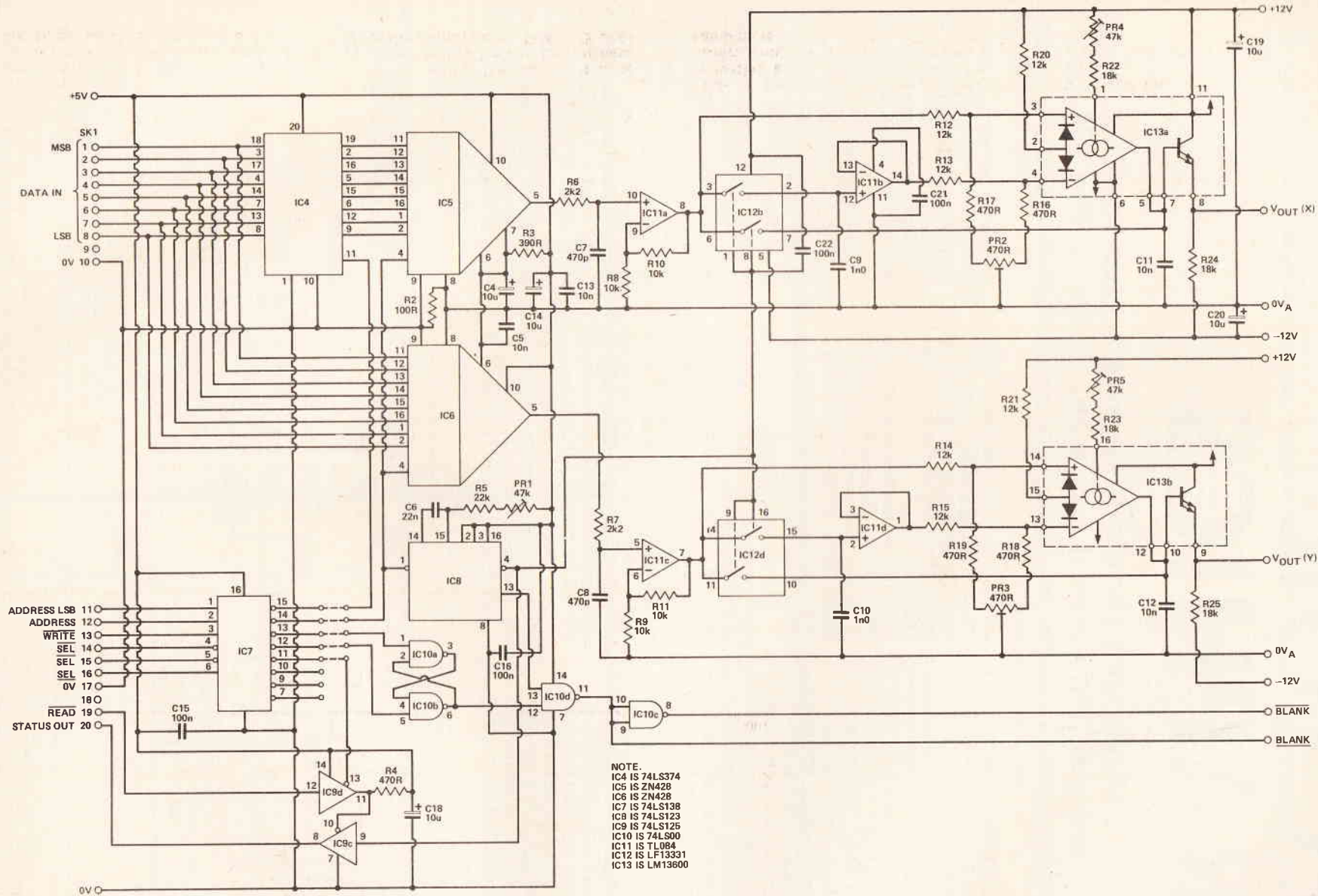


Fig. 2 Circuit diagram of the Graf-vec.

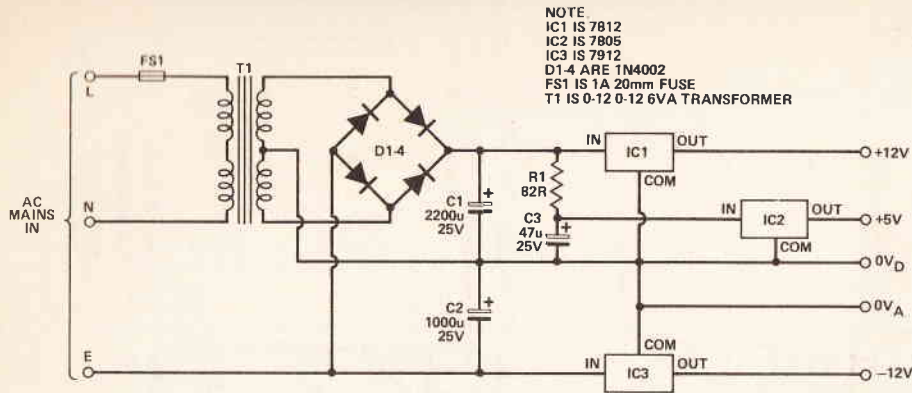


Fig. 3 Circuit diagram of the PSU.

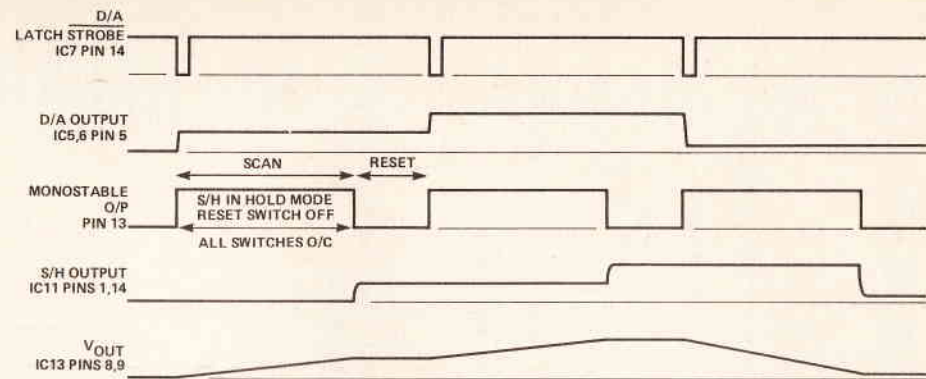


Fig. 4 Timing diagram of the Graf-vec.

How It Works

The Graf-vec consists of three major parts. The first of these is a straightforward stabilised power supply giving ± 12 V and +5 V at about 100 mA each. Only one transformer is used to save on cost and space. The output is regulated by three IC stabilisers which often need no heatsink in normal operation. However, R1 is provided to dissipate some of the excess power in the +5 V regulator, and a small piece of aluminium would not go amiss.

The second major part consists of the logic, timing and digital to analogue conversion. IC7 is a 74LS138, 1 of 8 decoder whose inputs are available at the input connector. This enables simple interfacing to some computer systems without additional circuitry. The outputs from this device are all available on the board via links and are used to enable the other logic functions. The first output drives the strobe input of a 74LS374 (IC4), which is an octal latch with three-state outputs. The outputs from the device are permanently on in this circuit and it is used to store the data corresponding to the X vector before it is loaded into the DAC (IC5).

The next output from IC4 has two uses. It drives the data input enable pins on the DACs (IC5 & 6) and it also drives the trigger input on IC8. ICs 5 & 6 are

ZN428 monolithic digital to analogue converters which accept data from the inputs when the enable pin is low and store it while the pin is high. They convert the digital data to a corresponding analogue output voltage in the range 0 to 2.55 V. Note that IC6 gets its data from the input data bus whereas IC5 gets it from the output of IC4.

IC8 is a dual monostable device only one part of which is used in this circuit. Its purpose is to provide the timing signals for the sweep generator, a display enable signal, and status indication back to the controller.

The next two outputs from IC7 are used to set or reset a simple latch made from two parts of IC10. An output from this latch is gated with the output from IC8 and enables or disables the display (if this facility is used.).

The final output from IC7 enables part of IC9 which is a 74LS125 Quad three state buffer. This transfers the logic level at SK1 pin 19 onto the enable pin of another section of IC9. If this is low, the logic state of IC8 Q output is impressed on SK1 pin 20. This indicates that the unit is ready to start display when the pin is high.

The final part of the Graf-vec is made up of two identical circuits. Each of these takes the output from a DAC (IC5 or 6)

and processes it to give the required output. We shall only explain one of these circuits as the other is exactly the same.

The output from the DAC comes via R6 and C7 which remove glitches and high frequency noise from the signal. It is then amplified by a factor of 2 by IC11a. This also provides a low impedance drive to the rest of the circuit.

Consider firstly the case when the Q output from IC8 is high (ie not triggered). The output from IC11a is connected via two of the four FET switches in IC12, an LF13331, to C9 and C11. This ensures that these capacitors are charged to a defined voltage before each sweep. Nothing further happens to this part of the circuit until the DACs are loaded with new information and IC8 is triggered. When this happens all the switches in IC12 are turned off. This isolates C9 which will hold its previous voltage for some time, and also removes the clamp on C11. The voltage on C9 is buffered by IC11b and applied via R13 to the inverting input of IC13. A new voltage now appears on the output of IC11a as the DAC has been updated. This is applied via R12 to the non-inverting input of IC13, an LM13600, which contains two transconductance amplifiers and two buffers. The trans-

conductance amplifiers provide an output current which is proportional to the difference of the two input currents, modified by currents into two other inputs.

In this circuit, one amplifier and buffer combination is used for each channel. The currents through R12 and R13 are subtracted and a current proportional to their difference flows into C11. Currents flowing through R20 and VR4, R22 determine what the actual gain will be. As the voltage on IC11a output is constant after its initial change and that on IC11b output is also constant, the resulting current flowing into C11 will be constant. The result of this is that C11 will charge linearly and will also tend to go in the direction of the voltage on IC11a output. In fact, when everything is set up correctly, the voltage on C11 will just reach the voltage on IC11a output as the monostable pulse ends. At this time the capacitor voltage will be clamped by the FET switches being turned on again. The capacitor voltage is buffered by buffers in the LM13600 before being sent out.

Finally it should be mentioned that R16,17 and VR2 form a balancing network and DC return path for the input currents and one of the control currents.

16514	11 10 00	LD DE,0010	:Scan counter = 256
17	PICOOT	06 0E	LD B, 0E :Points/scan = 14
19		21 A0 40	LD HL,40A0 :Start of data table = 16544
22	POINTOUT	7E	LD A,(HL) : Get "X" data
23		D3 1F	OUT (IF),A :Output "X" data
25		23	INC HL :Move data pointer
26	TESTIT	DB 1F	IN A,(1F) :Input status indicator
28		CB 7F	BIT A.7 :Isolate status bit
30		28 FA	JRZ (TESTIT) : Jump back if not ready (low)
32		7E	LD A,(HL) :Get "Y" data
33		D3 3F	OUT (3F),A :Output "Y" data
35		23	INC HL :Move data pointer
36		10 F0	DJNZ (POINTOUT):Repeat for all points
38		1B	DEC DE :Decrement scan counter
39		7A	LD A,D :Get scan count high byte
40		B3	OR A,E :OR with scan count low byte
41		20 E6	JRNZ (PICOOT) : Repeat if not zero
43		C9	RTS :Return to calling program

DATA LIST

16544	00 80 40 C0 7F 80 AE C0
	FE 80 7F 80 97 68 7F 50
	68 68 7F 80 7F 30 7F 80
	40 80 00 00

```

10 REM ( # :50RNDACS C IF .70
4 NEW TAN XXXXXXXXXXXXXXXXXXXXXXXX
XXXXXXXXXX
15 FAST
17 LET X=10
18 LET Y=X
30 POKE 16545,X
35 POKE 16553,X
40 LET X=X+Y
41 IF X>235 OR X<15 THEN LET Y
= (-1)*Y
45 GOTO 20
50 FOR K=16514 TO 16575
60 PRINT K,
70 INPUT A$
75 IF A$="" THEN STOP
80 IF LEN A$<>2 THEN GOTO 70
90 LET A=CODE (A$(1 TO 1))
100 LET B=CODE (A$(2 TO 2))
110 LET C=CODE "F"
120 LET D=CODE "0"
130 IF A>C OR A<D OR B>C OR B<D
THEN GOTO 70
140 POKE K,16*(A-D)+B-D
150 PRINT CHR$ A;CHR$ B
160 NEXT K

```

Table 2 ZX81 BASIC program. Note that you must go to line 50 to enter data and RUN to display.

Table 1 Z80 machine code demo program.

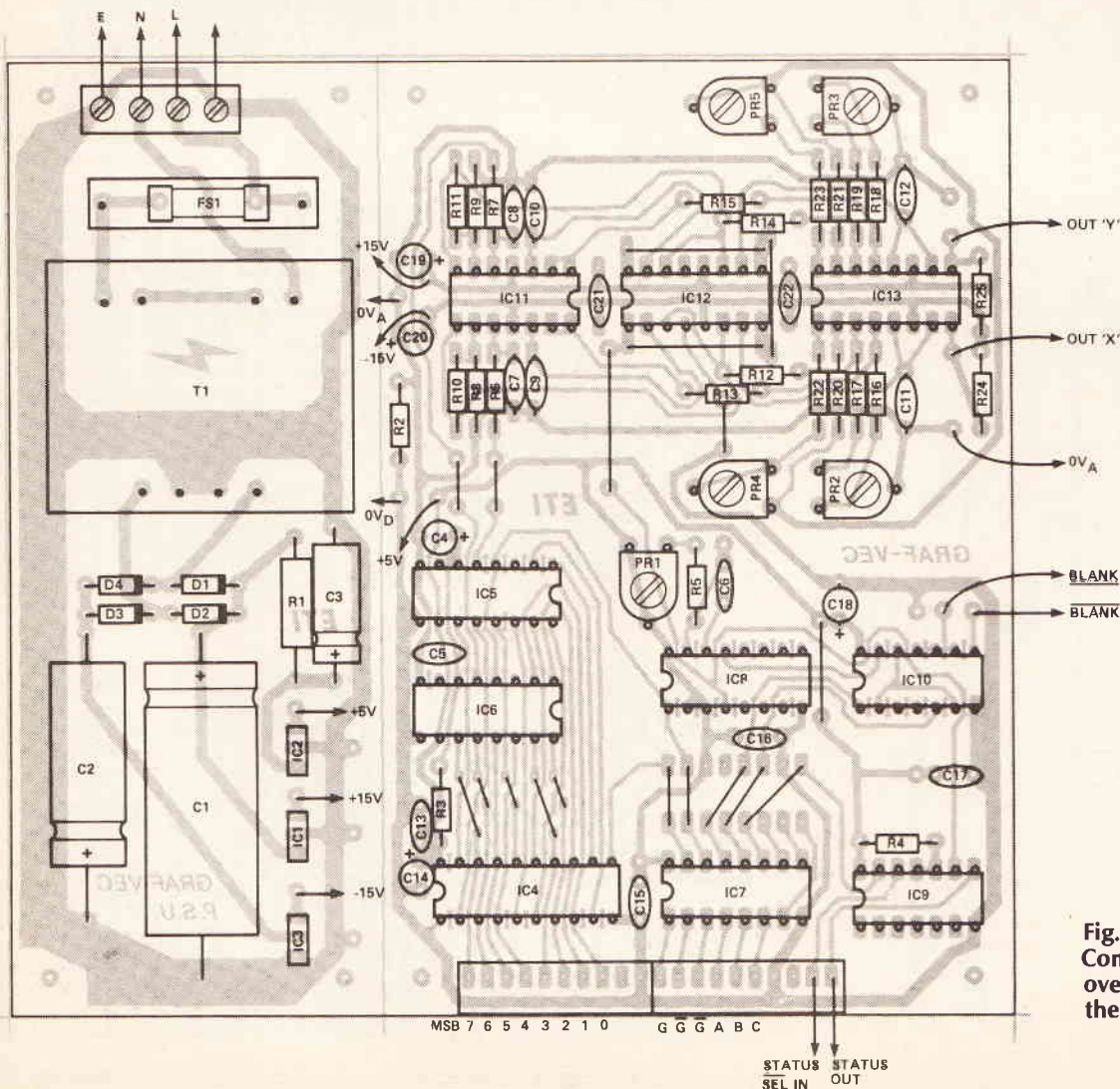
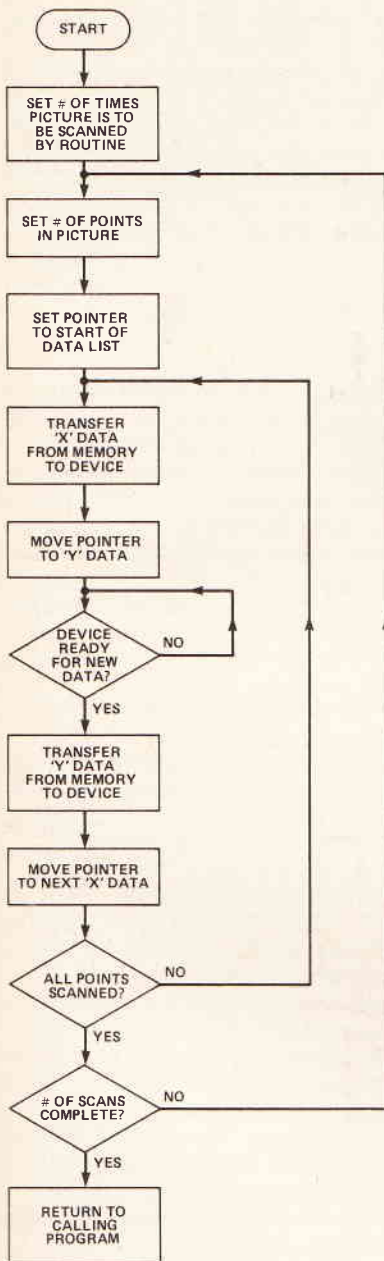


Fig. 5 (left) Component overlay of the PCB.

Fig. 6 (opposite) Flow chart showing how the display is formed.

PROJECT : Vector Graphics



latch, but the second byte should only be put in after the status bit is detected as high as this will start the next scan.

When the second byte of a new vector is written in, the logic section generates a 400 us enable pulse for the linear scan generators. This allows them to generate the linear voltage ramps which eventually move the spot around on the oscilloscope or other display device.

Once the 400 us pulse has finished, the linear scan generators are set up ready for the next vector and the display enable or blank output will go low. If you have the facility available, this can be used to blank the display between vector scans or, by means of the internal latch accessible by writing to two further addresses, the display can be turned on and off to allow you to move position without drawing a line.

The Linear Scan Generator

This is the heart of the whole system and is basically an integrator. Before each scan starts, the output voltage and the voltage stored on a sample and hold circuit are clamped to the current output from the D to A circuits. When a scan starts, the sample and hold circuit changes to its hold function and the output is unclamped. Since the output is closely associated with the integrator capacitor it does not change immediately.

The D to A circuit now changes its output voltage to the new value and a current is generated which is proportional to the difference between the old and new input voltages. This current is used to charge the integrator capacitor and will

do so at a constant rate. This gives a linear voltage ramp between the old output voltage and (if set up properly) the new one.

At the end of the scan pulse the sample and hold circuit and the output voltages are again clamped in readiness for the next scan. Note that while in the clamped state there is ideally no current flowing in the output circuit of the current generator as its input voltages are equal.

Semi-Solid Section

This is about the interface between the hardware described in this project so far and the software needed to make it do anything interesting. Fig. 6 shows in flow chart form the actions needed to form the display. In order to prevent a lot of flicker, the routine scans all the points in the display many times each time it is called. The main cause of any residual flicker is the relatively slow response of the BASIC program which calls it. If this too were in machine code a very smooth display could result.

Table 1 shows how the flow chart is implemented in Z80 code while Table 2 (up to line 45) is the ZX81 basic program which is used to control it. Lines 50 onward are a simple program which allows hexadecimal codes to be typed into the machine which are then held in the REM statement in line 10.

For initial entry of the machine code, alter line 50 to read:—

50 FOR K=16514 TO 16543

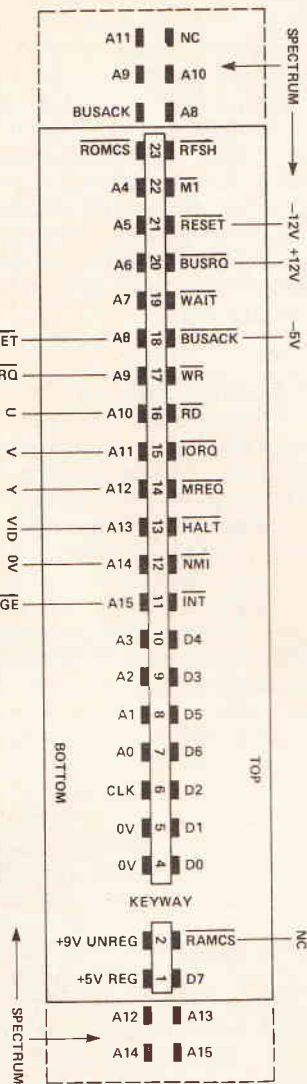
Then you can run the program from line 50 and input the program code. Changing line 50 back again will let you type in the data for the picture. The format for typing hex numbers in is two charac-

Parts List

Resistors (1/4 W Carbon film unless otherwise stated)						
R1	82R 1W	C2	1,000	uF 25V axial electrolytic	IC5,6	ZN428
R2	100R	C3	47	uF 25V axial electrolytic	IC7	74LS138
R3	390R	C4,14,18,19,20	10	uF 25V Tant. Bead	IC8	74LS123
R4,16,17,18,19	470R	C5,13	10	nF ceramic disc	IC9	74LS125
R5	22K	C6	22	nF polycarbonate	IC10	74LS00
R6,7	2K2	C7,8	470	pF ceramic	IC11	TL084
R8,9,10,11	10K	C9,10	1	nF polycarbonate	IC12	LF1331
R12,13,14,15,20,21	12K	C11,12	10	nF polycarbonate	IC13	LM13600
R22,23,24,25	18K	C15,16,17,21,22	100	nF ceramic	D1,2,3,4	1N4002
VR1,4,5	47K min. horizontal preset					
VR2,3	470R min. horizontal preset	Semiconductors				
Capacitors		IC1		1N4002	Miscellaneous	
C1	2,200 uF 25V axial electrolytic	IC2		7805	T1	0-12, 0-12 V 6 VA PCB mount mains transformer
		IC3		7915	FS1	1 A, 20 mm fuse + PCB mount holder
		IC4		74LS374	SK1	2 off, 10 way 0.1 in pitch PCB connector

4 way, PCB mount mains screw connector; PCB; Small heatsink for IC2; 23 way double sided edge connector 0.1 in pitch; 16 way (min) or 20 way ribbon cable.

PROJECT : Vector Graphics



Grafcvc socket 1	
pins 1 - 8 (data in)	ZX81 D0 - D7
pins 10, 17 (0V)	OV
pin 11 (address LSB)	A5
pin 12 (address)	A6
pin 13 (WRITE)	WR
pin 14 (SEL)	A7
pin 15 (SEL)	IORQ
pin 19 (READ)	RD
pin 20 (status out)	D7

Fig. 7 The ZX81 and Spectrum edge connector.

Table 3 Connections to the ZX81.

ters 0 to 9, A to F followed by newline. Wrong characters or wrong number of characters will require re-entry of the correct ones. To abort this entry mode type a single space and newline. When first entered, line 10 can be REM with at least 64 characters after it.

While the development work for the project was done on a Z80 system, there is no reason why any other processor could not be used. The only differences would be in the actual interface hardware and the machine code realisation of our flow chart.

There are 8 data lines, 7 control lines and one status output to the project. Normally the data lines will be connected to the controller's data bus. The status output line is from a three state buffer and can be connected to the data bus (we used bit 7). One of the remaining control lines is devoted to reading the status bit and must go low when a read operation is required (on a 6502 system it could be tied low permanently as the read and write are controlled by the same line). Of the remaining 6 control lines, one must be high and two must be low before anything happens. These would normally be used as select lines. The last three lines are used to select the operation to be carried out. One of these should be the R/W or similar function while the others will be simple address lines to select the particular operation to be performed. Exactly how these various lines are connected will depend on your particular requirements but Table 3 shows how we did it for a ZX81.

Construction

This should cause no headaches as it is quite straightforward. First of all, decide whether you want to use the PCB as it is or to split it into two parts (it might be tricky to cut it once the parts are assembled!). Note that there are eighteen links on the main board and five on the power supply, and begin by inserting these, the resistors, and the IC sockets. We recommend the use of sockets if only because some of the devices cost well over a pound and are therefore worth protecting... Next, fit the smaller capacitors, potentiometers, and sockets, followed by the power supply diodes, resistor (mounted 6 mm above the board), larger capacitors, fuse, and mains connector. Finally, fit the mains transformer

and insert the ICs into their sockets. Check that the ICs and capacitors are mounted the right way round.

Test the power supply section fully before connecting it to the other board and BE CAREFUL, there is MAINS VOLTAGE present. If all is well, all that remains is to wire the PCB connectors to suit your microcomputer or whatever and then connect up.

Setting Up

If you have an oscilloscope at hand — you need one for the display — set up the sample driver program or something similar on your computer etc and check that you get negative going pulses on the outputs of IC7 pins 15, 14 and 11. (this could change if you use a different jumper pattern for a different computer interface.) Set VR1 to give a low pulse period of 400 us at pin 4 of IC8.

Check the outputs from IC13 with the oscilloscope. These should consist of straight line segments with no sudden jumps. If this is not the case, adjust VR2 and VR4 for the X channel and VR3 and VR5 for the Y channel. VR2 and VR4 are effectively offset controls which tend to have the effect of shifting the lines in one direction whereas VR3 and VR5 are gain controls which increase the slope of the lines in whichever direction they happen to be going. The proper setting of these controls is vital to the production of a good display. If you have difficulty setting them, set up the data in the display table to be 00,00,FF,FF etc. This will give a repeating full scale display.

When the controls have been set up reasonably, run the demonstration program and set the 'scope to X-Y mode. You should now have a moving display. Final trimming of the pots. may be made to clear up any defects visible. If you do not have an oscilloscope, connect up the device to whatever you are using for a display, set all pots to mid travel and run the demo program and tweak for best results.

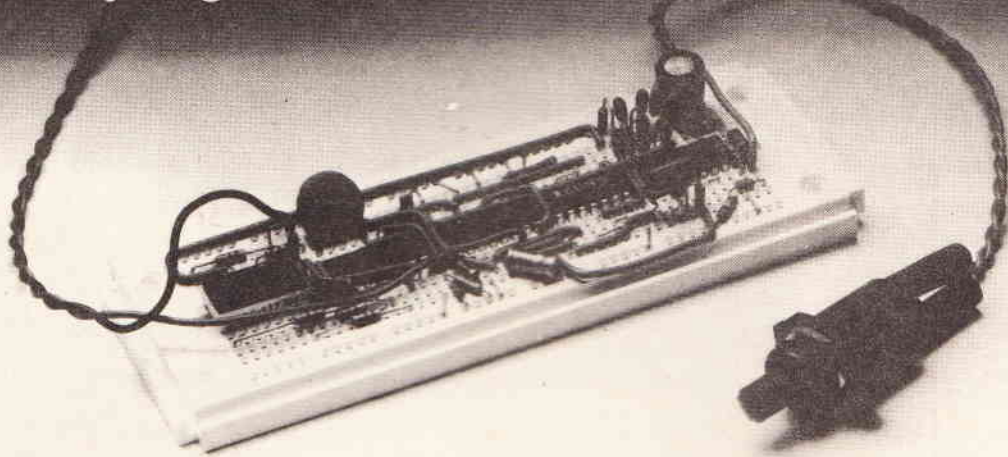
ETI

Buylines

There should be no problems with this lot. The LM12600, LF13331, and ZN428, etc are all available from Technomatic, among others. The transformer is available from Rapid, the PCB connectors from Ambit, and the mains screw connector from Electrovalue. The PCB is available from our PCB service on page 75.

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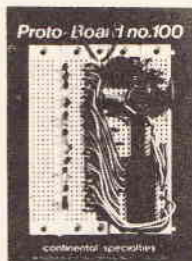
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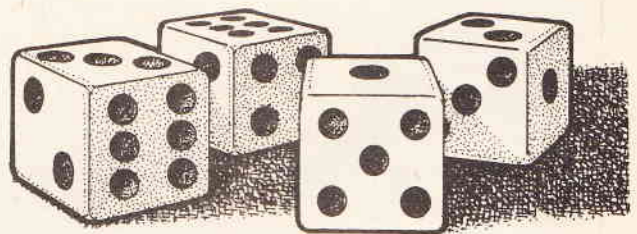
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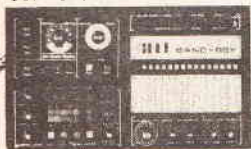
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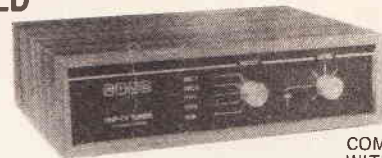
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ETI

SINCLAIR'S NEW POCKET TV

Why is there no love from Russia? Why are the French in tears? And why do Chinese gentlemen remain inscrutable? Ask Vivian Capel.

The reason is that these are among the very few places in which Clive Sinclair's new pocket TV will not work. Considering the many different TV standards in use throughout the world the fact that such exclusions are so few is certainly remarkable. Even more remarkable is that the set automatically adjusts itself to whatever standard is being received without any user switching at all. In fact the only external controls are the tuner and the on/off volume control.

The IC is unique in that it contains almost the whole of the TV circuitry; only the output stages and the tuner are external with just a few resistors and capacitors. This obviously reduces component costs considerably when the cost of originating the IC has been recovered, which it soon should be if the anticipated million sales a year materialise. Furthermore, it drastically cuts assembly costs, hence the price tag of under £80 which is about a third of the price of its nearest competitor, the Sony Watchman.

With the exception of the French 819-line system which is being phased out, most of the world has a 625-line standard, with the American continent and associated countries and islands having 525 lines. All the 625-line systems run at 50 Hz field frequency. Thus the line frequency for the 625-line standard is 15,625 Hz, while that of the 525-line system is 15,750. Five of the standards use AM sound while the rest employ FM. However, four of the five are obsolete systems (including our own 405-line system) which are either being dropped or have already disappeared. So apart from one, all current systems are FM. Much the same is true of vision modulation sense. The four obsolete systems use positive modulation but, with one exception, all the others are negative.

There are various differences in channel and vision bandwidths as well as vestigial sidebands, but these do not materially affect receiver design, they only produce minor differences in video response. There are also three basic colour systems but as all are compatible with black-and-white reception, they present no problems for a monochrome receiver.

This leaves us with one factor that does have an effect, the separation between sound and vision carriers. Apart from the obsolete systems there are four standards of separation, 4.5 MHz as used with all 525-line systems, 5.5 MHz, 6 MHz and 6.5 MHz which are used with various 625-line systems. This separation is important because the FM sound carrier and the AM vision carrier produce a beat frequency at the vision detector which is equivalent to their difference. After limiting to remove the AM video modulation, the result is an FM sound signal which is further amplified by sound IF stages at this new beat frequency. The arrangement is termed intercarrier sound, and it is obvious that any difference in the

spacing of the original sound and vision carriers will produce an equal difference in the sound IF frequency. So, TV standards using different spacings cannot normally be received with conventional sound IF circuits.

In order to cope with all these variables, the IC uses a voltage controlled oscillator which runs at a high multiple of the line frequency. Its frequency range can be set by an external resistor, but it is synchronised by the line sync pulses derived from the incoming video signal. The output is split into two paths, one of which is counted down by a logic stage to the line frequency. It is then converted from digital pulses to a suitable scanning waveform by a digital-to-analogue converter and fed to the line output stage. A line PLL stage compares the output of the logic circuit with that of the sync separator to provide a correction voltage for the oscillator. Thus whatever the incoming line frequency might be, the frequency of the oscillator will change to match it. From the line logic circuit there is a further countdown by the field logic stage to the field frequency. This too is locked to the incoming signal by means of the field sync pulses, so the field scan rate is dependant on the standard of the signal being received.

How, though, are the different vision/sound carrier spacings handled? The sound IF is set at 0.25 MHz, which means that there must be a means of converting the incoming intercarrier sound frequency to that value. This is done by another voltage-controlled oscillator which is also controlled by the line VCO. When the line oscillator is running at the 625-line standard the sound oscillator gives an output of 5.75 MHz, but when it is operating at 525 lines, the sound frequency is 4.75 MHz.

Just how it does this is not made very clear by the makers, but a possible method is to run the line oscillator at 8,000 times the line frequency which, at 15,625 Hz, the 625-line frequency, is 125 MHz, and at 15,750 Hz, the 525-line frequency, is 126 MHz. If the sound oscillator is set to run at 130.75 MHz, mixing with the line oscillator frequency will produce difference signals of $130.75 - 125 = 5.75$ MHz at 625 lines, and $130.75 - 126 = 4.75$ MHz at 525 lines. So, with an intercarrier signal of 4.5 MHz at 525 lines, and the oscillator producing 4.75 MHz, the result is a difference frequency of 0.25 MHz, which is the required IF. In the case of the 625-line system, a spacing and hence intercarrier frequency of 5.5 MHz together with the 5.75 MHz output from the oscillator again gives the 0.25 MHz IF. If, though, a spacing of 6 MHz is received (which is the intercarrier frequency for the U.K.) the same oscillator output of 5.75 MHz also produces a difference frequency of 0.25 MHz.

This leaves the 6.5 MHz separation signal out in the cold as the one not capable of being accommodated. It is found in the D, K, and L systems which are used in Russia, France, China, and several Eastern European countries

as well as a few African states. The L system, which is used in France, is the one having positive vision modulation and AM sound, so this is totally non-receivable, though the others could produce a picture without sound. However, as the produced difference signal is 0.75 MHz, which is the third harmonic of 0.25 MHz, the D and K systems might produce weak sound in the presence of a very strong signal.

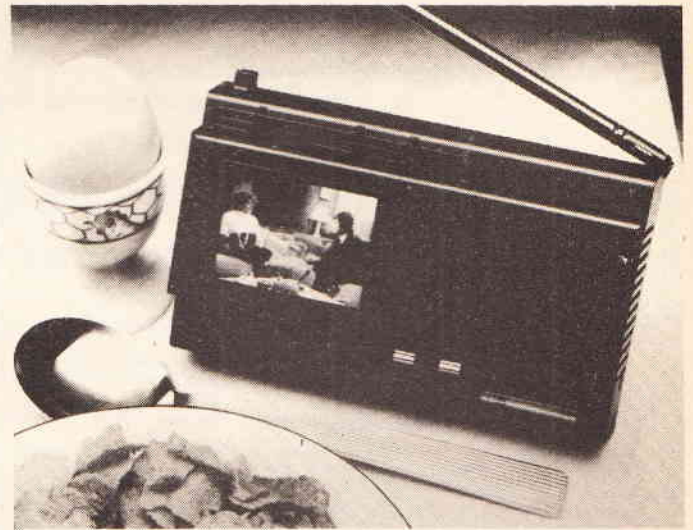
Output from the sound detector is taken from the chip to the volume control and from there back to the audio output stage which is also contained within the IC. Tuner output is applied to the vision IF stages which operate at the unusually high frequency of 230 MHz. This has the advantage of eliminating image-frequency interference from other UHF channels.

The tuner receives only UHF signals, and there are a number of countries that still have TV transmissions on VHF. Most of these also operate UHF transmitters as was the case in the UK, but for the benefit of those few areas that have only VHF services, a set with combined VHF/UHF tuner is planned.

The Flat Tube

The second major innovation in this remarkable set is the display tube. While LCD screens can offer compact low-current displays, the phosphor screen still takes some beating, if you can get around the awkward CRT shape which would be hard to fit into pocket TVs.

Size of the Sinclair tube is 4 x 2 x 3/4 inches, and the screen is 2 inches wide. It is constructed from two pieces of glass, a front plate and a backing plate which is vacuum formed by a new method developed for the project. The screen is deposited on the inside surface of the back plate which means that the image is viewed through the front plate on the same side of the phosphor that the electrons strike. With normal tubes viewing takes place through the layer of phosphor with attendant loss of light. Thus a much brighter picture is obtained for the same power dissipated, or conversely, lower power is required to give a picture of similar brightness as a conventional tube. Actual brightness is from two to three times greater.



Half of the width of the device is occupied by the screen, the other half accommodating the gun and deflector plates. These are mounted so that the electron beam is parallel to the screen surface, at least at the start. To strike the screen, it must be bent sideways, but this cannot be a gradual bend which would make it strike at a narrow angle as this would produce an elliptical spot, like a torch beam striking the ground at an acute angle. Such a spot would reduce the definition of the picture. To minimise this effect a strong electrostatic field is formed in front of the screen. A positive EHT potential is applied to a conductive coating behind the phosphor which attracts the beam, and a repelling negative potential is given to a conductive transparent layer of tin oxide on the front plate. As the beam enters the region between them it is deflected suddenly toward the screen at an angle which makes it strike the screen almost perpendicularly, giving a virtually round spot.

Another problem involving focus is caused by the unequal lengths of the beam path from the nearside to

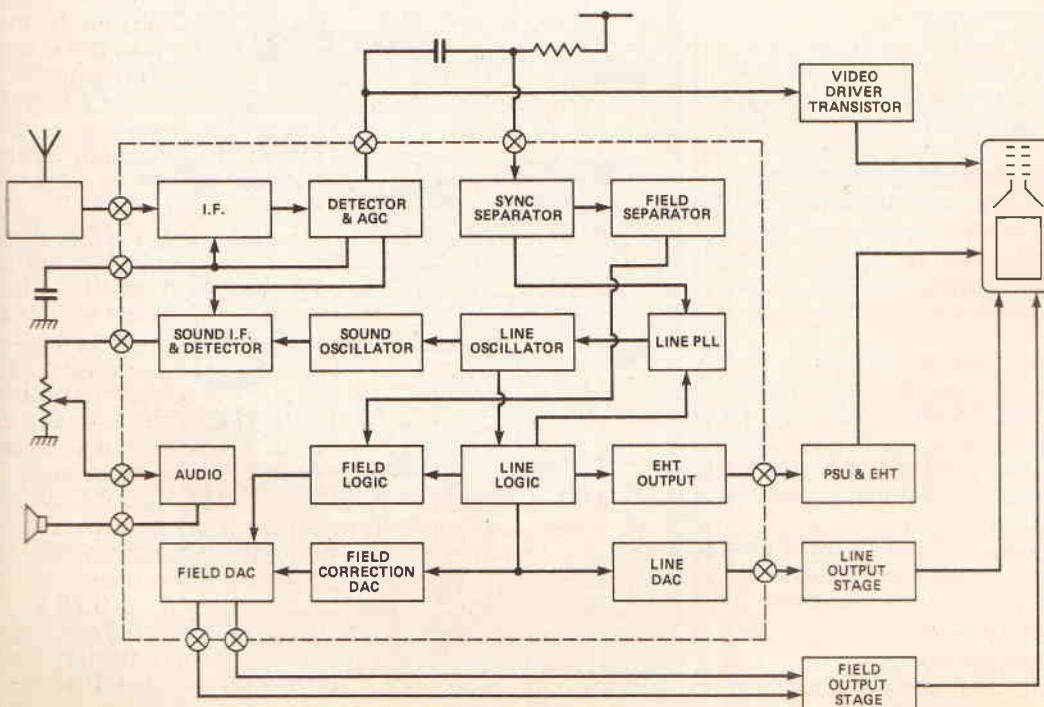


Fig. 1 Block diagram of the receiver. Everything within the dotted line is contained on the single IC.

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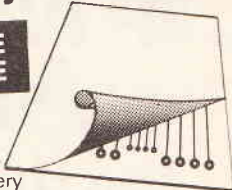


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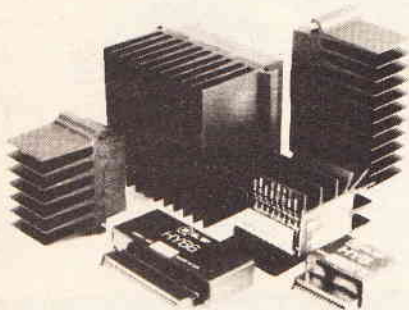
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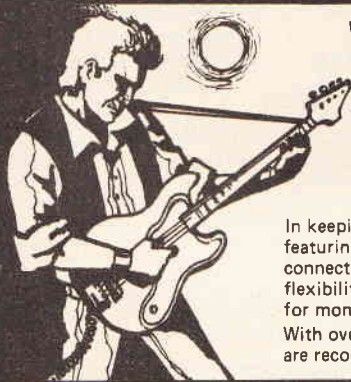


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			T.H.D. Typ at 1KHz	I.M.D. 60Hz/7KHz 4:1				
HY30	15	4-8	0.015%	<0.006%	± 18	76 x 68 x 40	240	£8.40
HY60	30	4-8	0.015%	<0.006%	± 25	76 x 68 x 40	240	£9.55
HY6060	30 + 30	4-8	0.015%	<0.006%	± 25	120 x 78 x 40	420	£18.69
HY124	60	4	0.01%	<0.006%	± 26	120 x 78 x 40	410	£20.75
HY128	60	8	0.01%	<0.006%	± 35	120 x 78 x 40	410	£20.75
HY244	120	4	0.01%	<0.006%	± 35	120 x 78 x 50	520	£25.47
HY248	120	8	0.01%	<0.006%	± 50	120 x 78 x 50	520	£25.47
HY364	180	4	0.01%	<0.006%	± 45	120 x 78 x 100	1030	£38.41
HY368	180	8	0.01%	<0.006%	± 60	120 x 78 x 100	1030	£38.41

Protection: Full load line. Slew Rate: 15V/ μ s. Risettime: 5 μ s. S/N ratio: 100db. Frequency response (-3dB) 15Hz - 50KHz. Input sensitivity: 500mV rms. Input Impedance: 100K Ω . Damping factor: 100Hz >400.

PRE-AMP SYSTEMS

Module Number	Module	Functions	Current Required	Price inc. VAT
HY6	Mono pre amp	Mic/Mag. Cartridge/Tuner/Tape/Aux + Vol/Bass/Treble	10mA	£7.60
HY66	Stereo pre amp	Mic/Mag. Cartridge/Tuner/Tape/Aux + Vol/Bass/Treble/Balance	20mA	£14.32
HY73	Guitar pre amp	Two Guitar (Bass Lead) and Mic + separate Volume Bass Treble + Mix	20mA	£15.36
HY78	Stereo pre amp	As HY66 less tone controls	20mA	£14.20

Most pre-amp modules can be driven by the PSU driving the main power amp. A separate PSU 30 is available purely for pre amp modules if required for £5.47 (inc. VAT). Pre-amp and mixing modules in 18 different variations. Please send for details.

Mounting Boards

For ease of construction we recommend the B6 for modules HY6-HY13 £1.05 (inc. VAT) and the B66 for modules HY66-HY78 £1.29 (inc. VAT).

POWER SUPPLY UNITS (Incorporating our own toroidal transformers)

Model Number	For Use With	Price inc. VAT
PSU 21X	1 or 2 HY30	£11.93
PSU 41X	1 or 2 HY60, 1 x HY6060, 1 x HY124	£13.83
PSU 42X	1 x HY128	£15.90
PSU 43X	1 x MOS128	£16.70
PSU 51X	2 x HY128, 1 x HY244	£17.07

Model Number	For Use With	Price inc. VAT
PSU 52X	2 x HY124	£17.07
PSU 53X	2 x MOS128	£17.86
PSU 54X	1 x HY248	£17.86
PSU 55X	1 x MOS248	£19.52
PSU 71X	2 x HY244	£21.75

Model Number	For Use With	Price inc. VAT
PSU 72X	2 x HY248	£22.54
PSU 73X	1 x HY364	£22.54
PSU 74X	1 x HY368	£24.20
PSU 75X	2 x MOS248, 1 x MOS368	£24.20

Please note: X in part no. indicates primary voltage. Please insert "0" in place of X for 110V, "1" in place of X for 220V, and "2" in place of X for 240V.

ILP Electronics Ltd., Dept 2, Graham Bell House, Roper Close, Canterbury CT2 7EP, Kent, England.
Telephone: (0227) 54778 Technical (0227) 64723. Telex: 965780.

MOSFET MODULES

Module Number	Output Power Watts rms	Load Impedance Ω	DISTORTION		Supply Voltage Typ	Size mm	WT gms	Price inc. VAT
			T.H.D. Typ at 1KHz	I.M.D. 60Hz/7KHz 4:1				
MOS 128	60	4-8	<0.005%	<0.006%	± 45	120 x 78 x 40	420	£30.41
MOS 248	120	4-8	<0.005%	<0.006%	± 55	120 x 78 x 80	850	£39.86
MOS 364	180	4	<0.005%	<0.006%	± 55	120 x 78 x 100	1025	£45.54

Protection: Able to cope with complex loads without the need for very special protection circuitry (fuses will suffice).

Slew rate: 20V/ μ s. Rise time: 3 μ s. S/N ratio: 100db

Frequency response (-3dB): 15Hz - 100KHz. Input sensitivity: 500mV rms

Input impedance: 100K Ω . Damping factor: 100Hz >400.

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Mono Power Booster Amplifier to increase the output of your existing car radio or cassette player to a nominal 15 watts rms.

Very easy to use.

£9.14 (inc. VAT)

Robust construction.

Mounts anywhere in car.

Automatic switch on.

Output power maximum 22w peak into 4 Ω .

Frequency response (-3dB) 15Hz to 30KHz. T.H.D. 0.1% at 10w 1KHz

S/N ratio (DIN AUDIO) 80dB. Load Impedance 3 Ω .

Input Sensitivity and Impedance (selectable) 700mV rms into 15K Ω 3V rms into 8 Ω .

Size 95 x 48 x 50mm. Weight 256 gms.

C1515

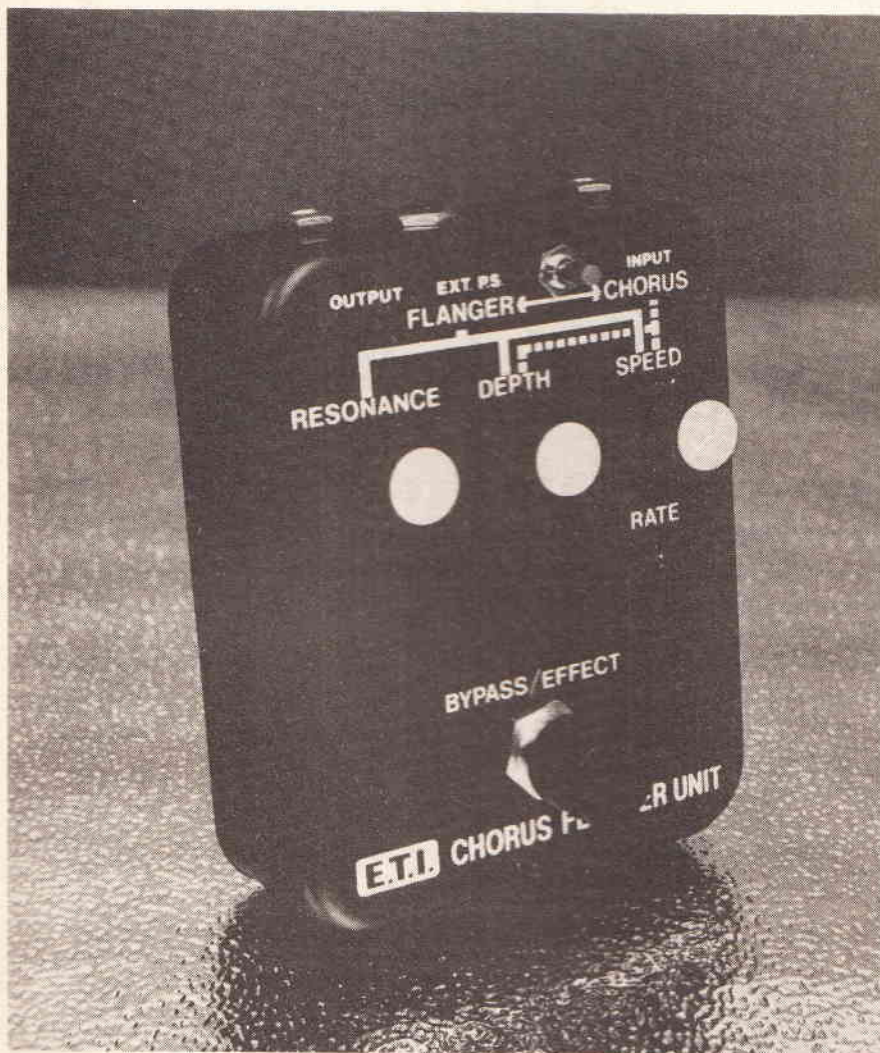
Stereo version of C15.

£17.19 (inc. VAT)

Size 95 x 40 x 80. Weight 410 gms.

CHORUS/ FLANGER UNIT

Tim Orr returns to the pages of ETI with a project to make your amplifier see double — a chorus/flanger.



The Chorus/Flanger unit is a device for processing musical and other signals to produce a wide range of effects. The electronics have been optimised for an electric guitar input but the unit can run equally well from line level signals (−6dBm) and high output microphones.

The chorus effect simulates a second instrument, which is producing the same sound as the input signal, but which is slightly delayed in time. This tends to generate the illusion of a second instrument and also enriches the overall sound quality. If a relatively fast (10Hz) time modulation is used, then genuine vibrato is generated. Flanging is a very dramatic colouration of the input sound. An instrument played through a flanger sounds like it is being heard in a drain pipe, the size of which is changing!

Flanging, chorus and vibrato are all time delay effects, and so their implementation is relatively simple if we use a bucket brigade delay line, Fig. 1. Voltages presented to the input of the delay line are sampled and then converted into small quantities of charge. These charges are passed along several hundred electronic 'buckets' until they reach the output, whereupon they are reconverted back into the original voltage. This process takes time, in fact the time delay is equal to the number of buckets divided by the speed at which the charge is passed along the line. The signal recovered at the other end very closely resembles the input signal except for a small amount of noise and distortion (it's an imperfect world).

As this is a sampled information system we must sample the input signal much more frequently than the highest frequency compon-

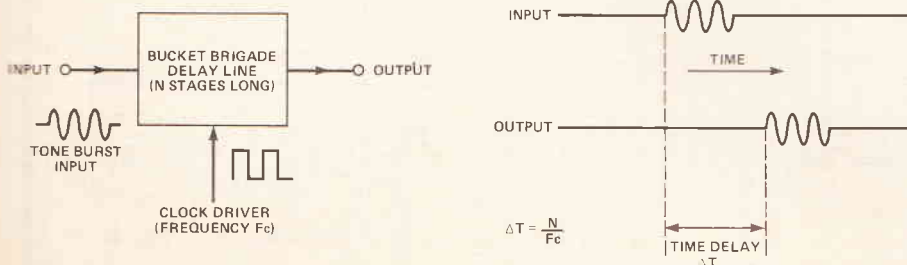
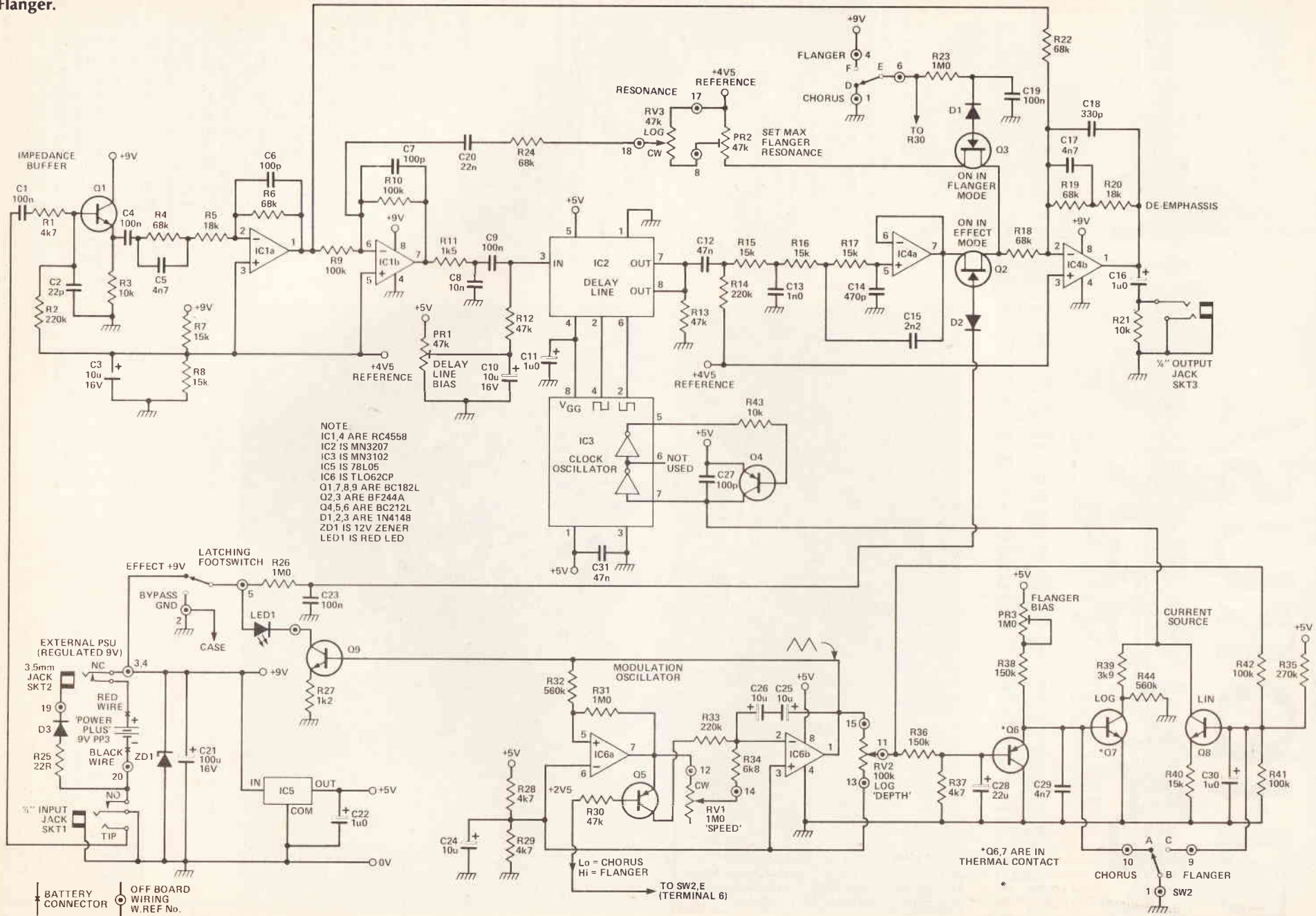


Fig. 1 The basic principle of producing a time delay.

Fig. 5 Circuit diagram of the Chorus/ Flanger.



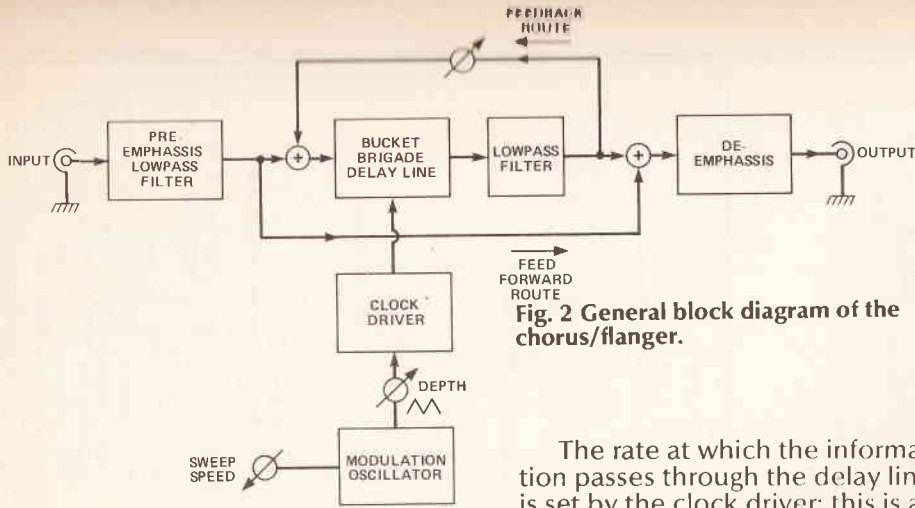


Fig. 2 General block diagram of the chorus/flanger.

The rate at which the information passes through the delay line is set by the clock driver: this is a high frequency oscillator which can be frequency modulated. The delay line (MN3207) has a delay length of 512 buckets, so a clock frequency of 512 kHz will produce a delay time of 1 millisecond. The modulation oscillator is used to produce slowly-varying time delays of variable speed and depth.

The chorus-flanger unit has been configured to look like a comb filter, Fig. 3. This is a filter

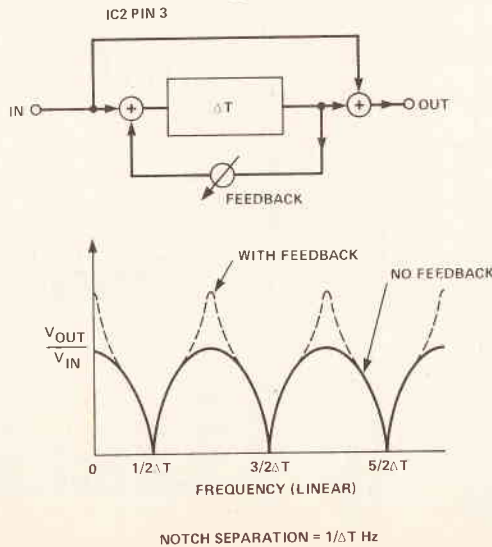


Fig. 3 A basic time delay comb filter.

elements of the input signal. By doing this, we can avoid the dreaded aliasing distortion (which sounds like ring modulation) and hope to recover the input signal with some degree of integrity.

The general block diagram of the chorus-flanger unit is shown in Fig. 2. The low-pass filter at the front end of the unit limits the input bandwidth and so helps to avoid any aliasing problems. The low-pass on the output recovers the delayed signal and rejects unwanted high frequency clock and noise signals.

The audio signal is given a treble lift (pre-emphasis) at the front end of the unit and a treble cut (de-emphasis) at the output. This helps to produce a better signal to noise ratio throughout the unit: most natural sounds have an energy spectrum that drops off very rapidly with increasing frequency, so by giving a frequency lift to these parts of the spectrum, more information can be elevated above the noise floor of the delay line. At the output end of the system, the de-emphasis restores the overall frequency response back to a flat one, but also suppresses high frequency noise from the delay

HOW IT WORKS

Q1 forms a conventional high-impedance buffer: experience has shown that electronic guitars sound better when presented with a fairly high input impedance.

IC1a performs signal pre-emphasis, lifting all frequencies above about 500 Hz; IC1b performs the low-pass anti-aliasing filtering, as well as mixing the fed-back proportion of the delayed output (which comes in via RV3, R24 and C20).

PR1 sets the DC bias level of signal going to the input of the bucket-bridge device; this is needed to obtain minimum signal distortion. The output from IC2 is recovered by the low-pass filter around IC4a, and passed to the FET signal switch, Q2 (FETs are used rather than mechanical switches to save loud-speaker cones!). Q2 allows the signal to pass except when the unit is in the bypass mode.

Q3 is another FET signal switch, and when the unit is in the flanging mode, this feeds a proportion of the delayed signal back to the input via PR2, the resonance control RV3, R24 and C20. At the same time, the fed-forward signal and the delayed signal are combined by IC4b, which also performs the de-emphasis. From here the signal is passed to the output.

IC6 forms a simple triangle/square-wave oscillator. RV1 controls the oscillation speed. Q5 is used to limit the low

frequency range of the oscillator when in the chorus mode.

Q9 is used to drive the panel LED. When the effect is selected (via the footswitch) the LED will light up and flash at the modulation rate.

IC3 and Q4 form the clock oscillator for the delay line. C27 is charged up by either Q7 or Q8, both of which act as current sources. When pin 7 of IC3 drops below about +2.5V, pin 5 of the same IC goes low, which turns on Q4, which discharges C27 back up to +5V. Thus the circuit oscillates at a rate determined by the size of the current sink from either Q7 or Q8. In the chorus mode Q8 generates a linearly varying current over a maximum two-to-one range. C30 limits this sweep at faster rates. In the flanger mode, Q6 and Q7 generate an exponentially varying current over a seven-to-one range. Again the modulation depth is limited at fast rates by a capacitor, C28.

IC5 provides a stable +5V power supply for the modulation oscillator, clock oscillator and the delay line. Battery voltages droop with time! The battery starts life at about +9.5V and has an end of useful life at about 6.5V. For maximum battery life, plug in the effect unit only when it is needed and never leave it on over night. The ON/OFF switch is the input jack which has a switched earth pin. For infinite battery life use a mains power supply (a PP3 eliminator)!

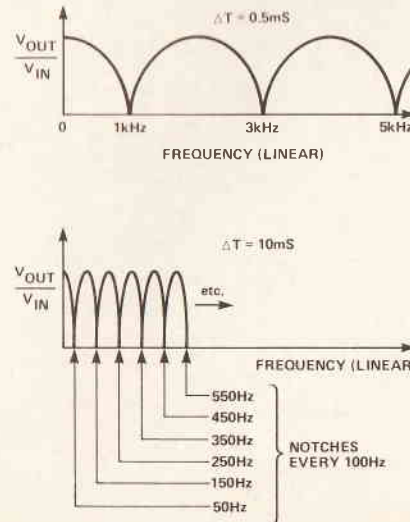


Fig. 4 Comb filter frequency responses for different time delays.

with a frequency response that is full of notches, and which looks like the teeth of a comb! When the delayed signal is 180° out of phase with the direct signal, then cancellation will occur and a notch in the frequency response is generated. These notches are linearly spaced with a separation of 1/(the time delay). Feedback around the delay line (used in flanging) makes the comb response much more peakey when the phase shift around the delay line is zero. Short time delays produce few notches and long time delays produce several, Fig. 4. Note that the frequency separation of the notches is linearly proportional to the clock frequency.

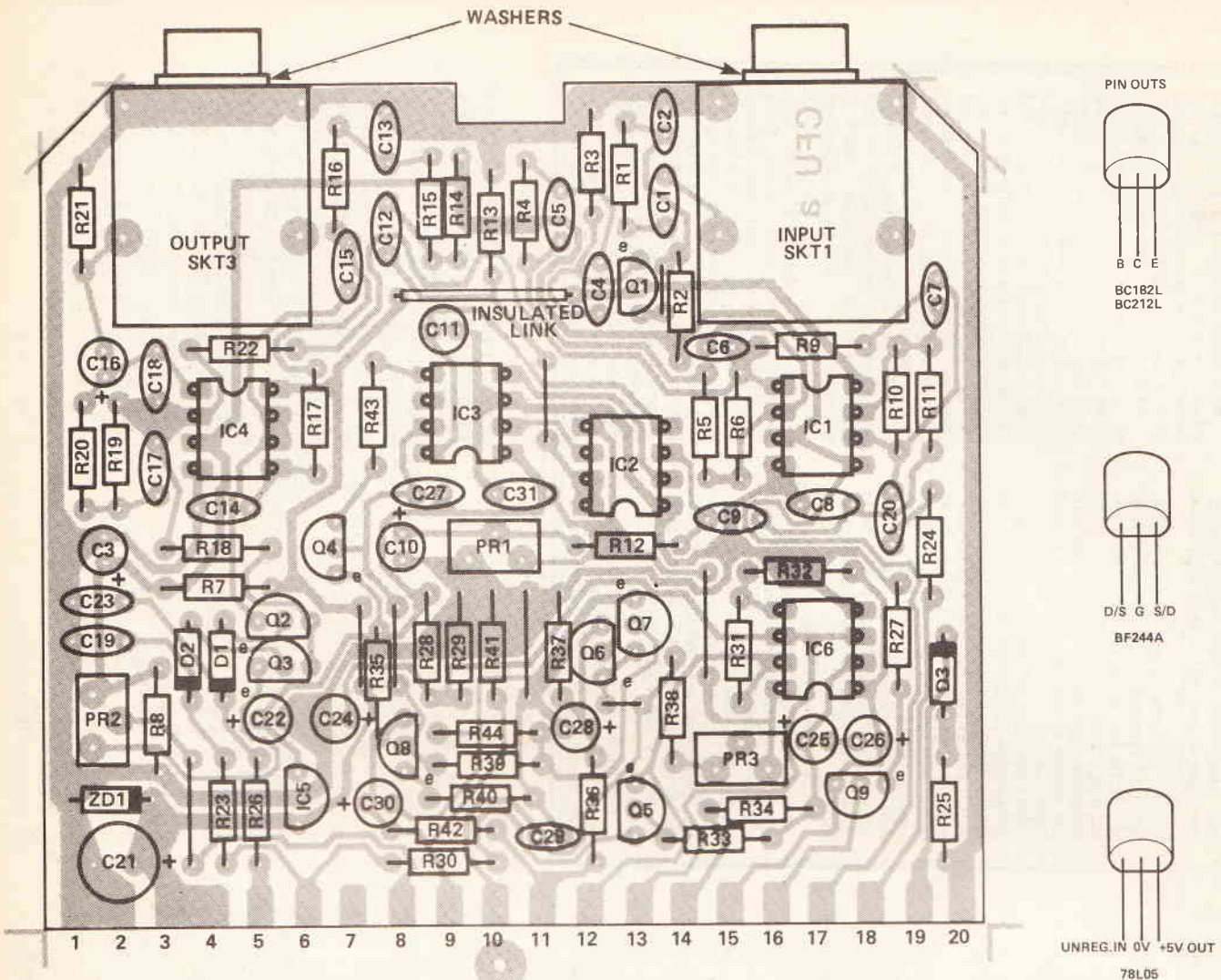


Fig. 6 Overlay diagram of the PCB for the Chorus/Flanger

PARTS LIST

RESISTORS (all 1/4W 5%)

R1	4k7
R2	220k
R3	10k
R4,6	68k
R5	18k
R7,8	15k
R9,10	100k
R11	1k5
R12,13	47k
R14	220k
R15,16,17	15k
R18,19,22,24	68k
R20	18k
R21	10k
R23,26,31	1M0
R25	22R
R27	1k2
R28,29,37	4k7
R30	47k
R32	560k
R33	220k
R34	6k8
R35	270k
R36,38	150k
R39	3k9
R40	15k
R41,42	100k
R43	10k
R44	560k

POTENTIOMETERS

RV1	1M0 reverse logarithmic
RV2	100k logarithmic
RV3	47k reverse logarithmic
PR1,3	47k preset
PR2	1M0 preset

CAPACITORS

C1,4,9	100n polyester
C2	22p ceramic
C3,10	10µ 16V PCB electrolytic
C5	4n7 polyester
C6,7	100p ceramic
C8	10n ceramic
C11,16	1µ0 63V PCB electrolytic
C12	47n polyester
C13	1n0 polyester
C14	470p ceramic
C15	2n2 polyester
C17	4n7 polyester
C18	330p ceramic
C19	100n polyester
C20	22n polyester
C21	100µ 16V PCB electrolytic
C22,30	1µ0 63V PCB electrolytic
C23	100n polyester
C24,25,26	10µ 16V PCB electrolytic
C27	100p ceramic
C28	22µ 16V PCB electrolytic

C29	4n7 ceramic
C31	47n polyester

SEMICONDUCTORS

IC1,4	RC4558
IC2	MN3207
IC3	MN3102
IC5	78L05
IC6	TL062CP
Q1,7,8,9	BC182L
Q2,3	BF244A
Q4,5,6	BC212L
D1,2,3	1N4148
ZD1	BZY88-12V zener
LED1	0.2" red LED

MISCELLANEOUS

SKT1,3	1/4" mono switched jack sockets
SKT2	3.5 mm mono jack socket
SW1	latching footswitch SPCO plus cap
SW2	DPDT switch
PCB; knobs; PP3 battery connector; case; self-adhesive foam strip (for securing the PCB); 8-pin IC sockets (5 off); holder for LED; wire, solder, Gibson Les Paul Special, etc.	

PROJECT : Chorus/Flanger

Assembly And Setting Up

Assemble the PCB and connect to the controls as shown in Figs. 6 and 7. When testing is complete, the PCB is mounted in the box, supported by the jack sockets, with the foil side to the case bottom. Put some thin sticky-backed foam rubber on the inside of the case bottom to prevent shorts.

Table 1 shows various DC test voltages around the circuit and Fig. 8 shows some of the waveforms you should find using an oscilloscope. As regards the setting of the presets, you can just plug in, switch on and hope for the best and set the presets by trial and error, but if you do have access to

IC1,4, PIN 8	+9V (FOR BATT. OPERATION)
IC1, PINS 3,5	+4.5V APPROX
IC1, PINS 1,7	+4.5V APPROX*
Q1 EMITTER	+3.8V APPROX*
IC2, PIN 5	+5V
IC2, PIN 1	+5V
IC3, PIN 8	+4.67V
IC4, PINS 1,7	+4.5V APPROX*
IC6, PIN 8	+5V
IC6, PIN 3,6	+2.5V

* VOLTAGE WITH NO INPUT SIGNAL

Table 1 DC test voltages.

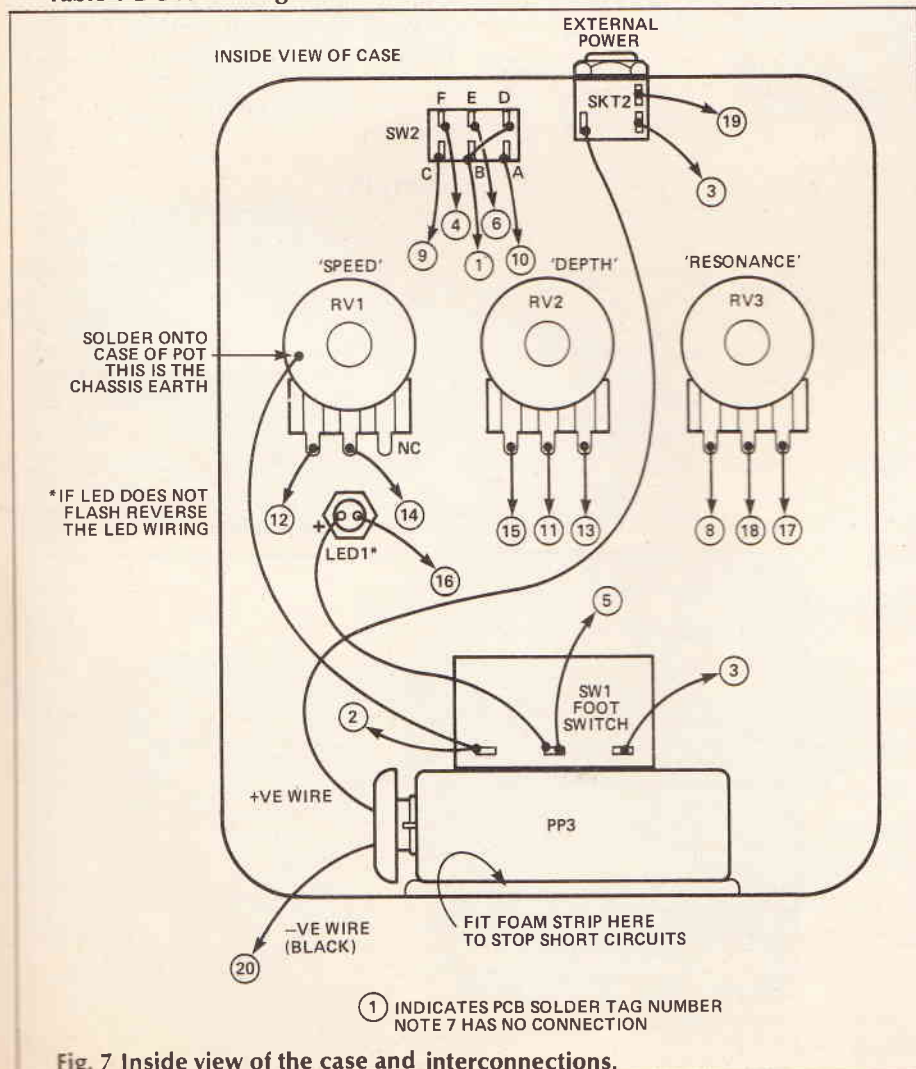


Fig. 7 Inside view of the case and interconnections.

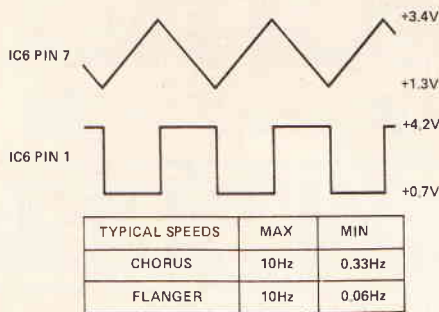


Fig. 8a Waveforms for the modulation oscillator; note that the voltage levels for IC6 are only approximate, as are the oscillator frequencies.

some test gear, here is the proper way to set up the unit.

Inject a 2.0 V peak-to-peak 500 Hz sinewave into the input socket, and select chorus on SW2 with the footswitch, SW1, set to effect. Set the rate control to maximum and the depth control to minimum. Using an oscilloscope, check that the undistorted signal is present at

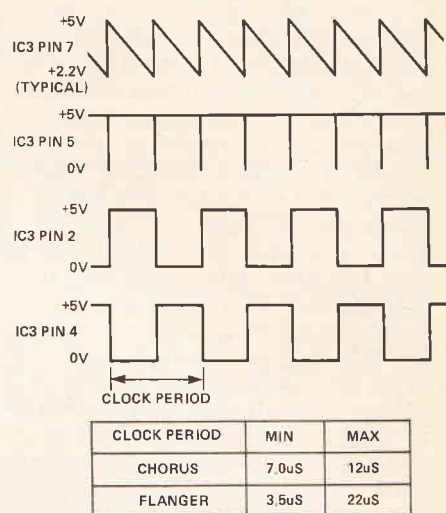


Fig. 8b Waveforms for the clock oscillator; select minimum depth (RV2) for these waveforms. The table shows the limits of the clock period for depth set to maximum and rate set to minimum; the preset PR3 should be adjusted to bring the oscillator into the range given for the flanger mode (with the flanging effect selected).

Q1 emitter, IC1 pins 1 and 7 and IC2 pin 3.

Set PR1 to its mid-way position and look at the signal present on IC2 pin 8; adjust PR1 until the signal is clipping symmetrically (see Fig. 9). Note that this signal will have a lot of high-frequency clock signal breakthrough: this is normal.

Examine the output at IC4 pin 7; this should be the same signal without the HF breakthrough. Reduce the input signal level to remove the clipping on this signal. Turn the depth control to maximum and the sinewave at IC4 pin 7 will be frequency modulated by the modulation oscillator; a mixture of this signal plus the direct signal should appear at IC4 pin 1.

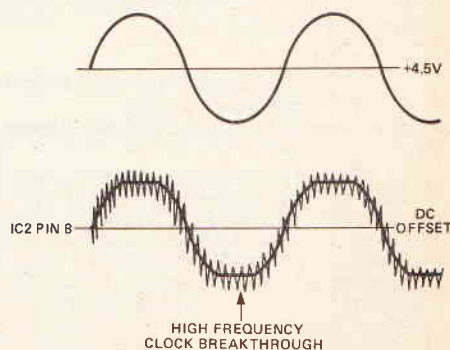


Fig. 9 Waveforms at the input and output of IC2.

PROJECT : Chorus/Flanger

The flanging effect is best tested with a 200 mV P-P square wave oscillating at 2 Hz. This excites the unit with two clicks per second. Set resonance to maximum, speed to minimum and SW2 to the flanger position (foot-switch SW1 should still be set to effect and not bypass). Listen to the output from the unit via a suitable amplifier, and adjust PR2 so that the output is a rich 'drainpipe' sound (you'll hear what we mean). If PR2 is set for too much feedback, the unit will oscillate; if this occurs back off the control a little.

For both chorus and flanging effects, the time modulation depth reduces as the modulation speed increases. The modulation depth at 10 Hz should produce a pleasant vibrato effect, caused by a small time delay sweep.

Power Supply

The unit consumes about 1mA. Using an Ever Ready PP3PP (power plus) for two hours per day, the expected battery life will be about 20 hours. If you leave the unit turned on over night, you will exhaust the battery. It is possible to use a rechargeable Nickel Cadmium PP3 battery. This has a shorter discharge life time of about 7 hours, but can be reused (charged/discharged) about 600 times! The purchase price of Nickel Cadmium batteries is about six times that of a standard PP3, and also you will need a charger unit. A non rechargeable alkaline PP3 battery (eg Duracell type) gives about four times the energy content of a zinc carbon PP3 but costs about twice as much.

A 9V battery eliminator can be used, the operating power is then derived from the mains. Note that the inner connection is +9V and the outer is 0V; if the polarity is reversed, D3 should prevent any damage to the chorus flanger, but the unit will not work.

BUYLINES

A full kit of parts for this project is available from Sola Sound Ltd, for £49.95 all inclusive. Alternatively, some of the more unusual parts are available as follows: PCB £1.15 inclusive; case (fully screened) £3.75 inclusive; MN3207/MN3102 (IC2 and 3) £13.80 the pair. All these prices include VAT and postage. Sola Sound Ltd may be found at 18 Barton Way, Croxley Green, Rickmansworth, Herts. (Note that the PCB will not be available through the ETI PCB service.)

EXTERNAL POWER UNIT
AMP & SPEAKER
GUITAR

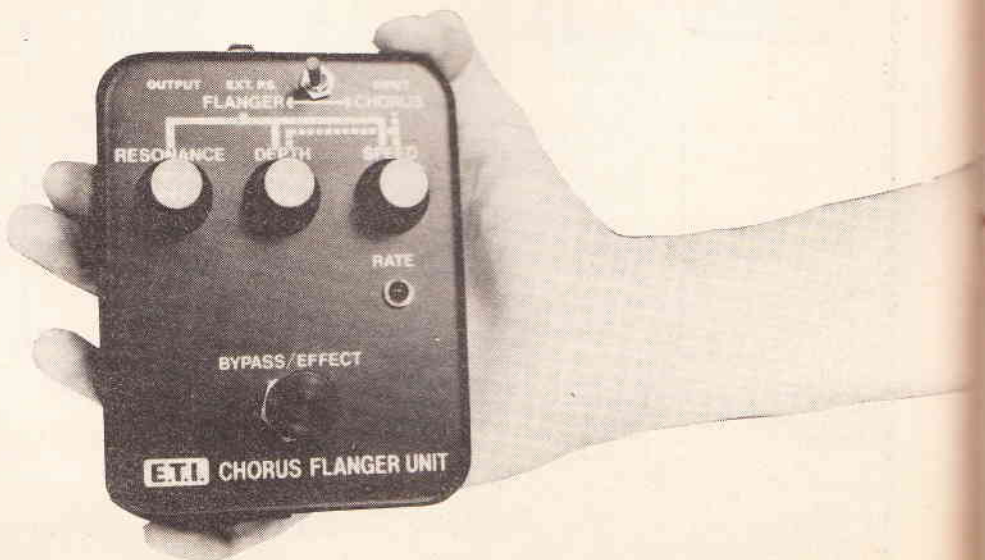
User Guide
 Plug in the guitar and the amplifier. Press the footswitch so that the LED is off. Turn up the guitar volume, set up the amplifier level and tune the guitar. This is the BYPASS mode.

Vibrato
 Set up the controls as shown, with SPEED and DEPTH at maximum. RESONANCE is inoperative. Press the footswitch so that the LED is flashing. Play the guitar. A fast (10Hz) vibrato will be heard. If necessary alter the guitar and amplifier levels. Adjust both controls for less depth and different vibrato rates.

Chorus
 Set up the controls as shown, with the DEPTH set to maximum and a SPEED setting of about 1 flash per second. RESONANCE is inoperative. Play the guitar. A "creamy" sound will be heard. Press the BYPASS footswitch and see how flat the original signal sounds. Go back to the effect and try some different SPEED and DEPTH settings.

Flanging
 Set up the controls as shown with DEPTH and RESONANCE to maximum and SPEED to minimum. Tap the guitar strings. A slowly sweeping "drain pipe" resonance will be heard. Try playing a melody with a rhythm that has the same period as the sweep time. Try other control settings.

RES DEPTH SPEED
 CHORUS
 RES DEPTH SPEED
 CHORUS
 RES DEPTH SPEED
 FLANGING



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The Broxbourne sales counter is operated under the auspices of David Scott from



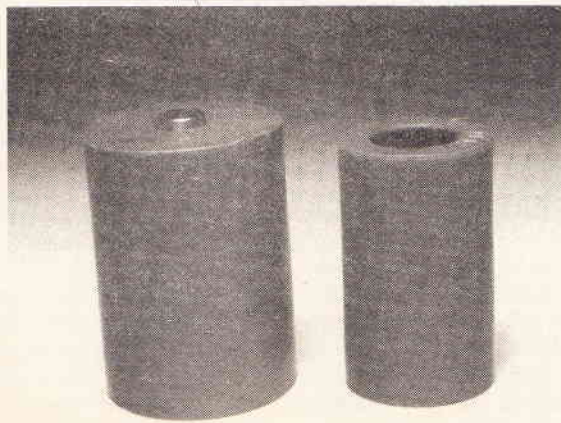
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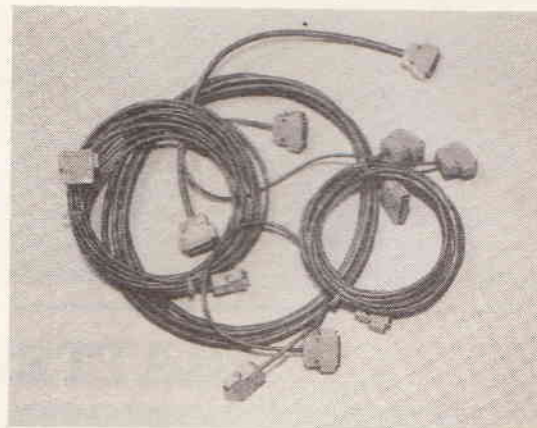
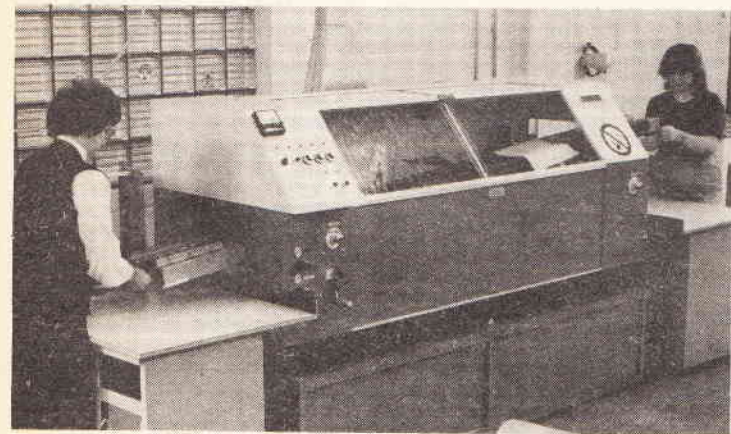
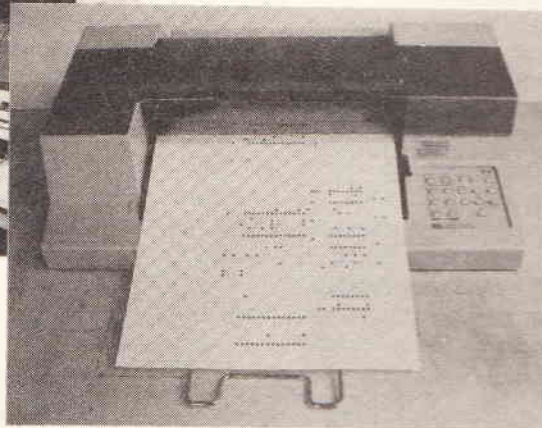
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Broxlea's energetic MD, Peter Telling, can provide on-site assessment of your requirements



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A. F. BULGIN INVEST IN THE FUTURE

The long established component firm consolidates its subsidiary activities.

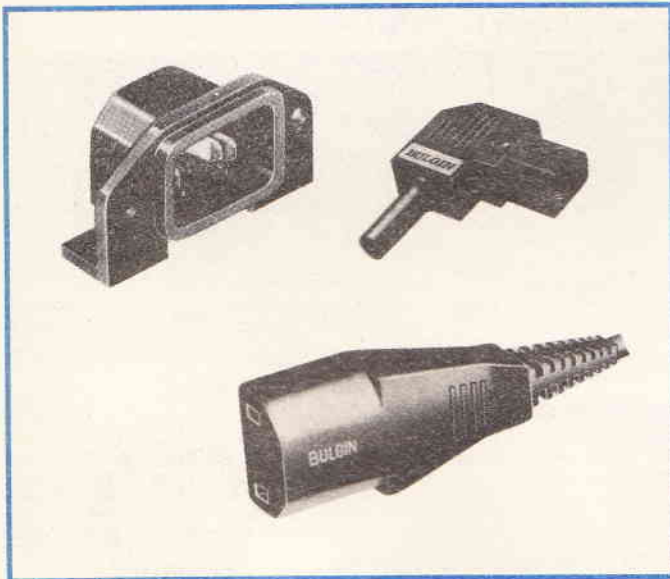
There are few participants in the electronics business who will not have come across some of the many different connectors, fuseholders, plugs, sockets, knobs etc., that are made by A. F. Bulgin & Co. PLC, of Bypass Road, Barking. 60 years in the business is unusual in electronics, and in order to establish plans that ensure the name of Bulgin will be carried forward through the next 60 years, Chairman Ronnie Bulgin and his board have decided that diversification is one of several moves to be made.

The distributive activities and associated skills of Ambit have been acquired to precede the formal consolidation of AFB's external business interests in Portsmouth (Solent Component

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Ambit's innovative REWTEL direct order placement system caused quite a stir in the distribution industry, since it demonstrated the first keyword index information and bulletin service, combined with direct on-line order interrogation facilities.



Hardware versatility

The product range for which A.F. Bulgin & Co. PLC has become most famous over the past 60 years is probably its range of connectors, fuseholders and panel hardware.

The popular IEC connector range is continually being updated. There are now PC mounting types, filter inlet sockets and many other variations on the theme. Although now largely replaced in mains voltage applications by the IEC families, the round plug

and socket series has been brought right up to date with the "Buccaneer" range of water resistant housings, offering a wide variety of connection options, including BNC coaxial, 3 and 6 pole types.

As with all the mains rated components, the fuseholders comply to the latest BS safety specifications to ensure acceptability of equipment and freedom from the unexpected shocks that can arise from the use of improperly designed parts.



OPENING HOURS

Consumer admin:

(0277) 230909 - 4 lines

Availability of goods Credit card orders

Ask for
(credit card sales) 9-5.30
Customer Service problems
with deliveries 10-12.30
Ask for 'Customer Service'

Industrial sales, admin & progress:

(0277) 231616 - 4 lines

Availability, price, telesales

Keith Collins 9-5.30
Claire Mackessy 9-5.30
Carol Lawton 9-5.30

Shop Sales

Brentwood Mon-Sat 9-5.30
Lunch 1.30-2.30
Broxbourne Mon-Fri 9-5.30
Sat 9-12.30
Portsmouth Mon-Sat 9-5.30



Apart from "own brand" products, A.F. Bulgin handle a number of agencies on behalf of overseas manufacturers of complementary products — most notably the superb range of control knobs from Ritel of Switzerland, a very large selection of which are available from Ambit stock and detailed in the current catalogue.

Many lines are custom manufactured, taking advantage of Bulgin's unrivalled experience, extensive in-house tooling facilities and automatic injection molding plant. If your firm requires either a variation on a standard theme, or a completely new type of small plastic/metal component, then let us quote you for supplying it from one of the few remaining sources of British component manufacturing expertise.

Telephone Timing



Help us to help you!

When calling our central sales and service departments at Brentwood, it would help us a great deal if you would observe the following timing. At present we tend to get all the calls arriving at peak periods, when other times the lines are deserted.

We get many reports of difficulty in getting through, but it's not for lack of incoming lines! Please use the numbers designated for the nature of your enquiry, it is sometimes not possible to transfer between industrial and consumer sales due to the volume of telephone traffic.

The peak time for consumer telesales is 10.15—10.45 and 2.30—4pm. If you can avoid these, then so much the better for you and us. Telesales operate Monday to Saturday, 9.00am to 5.30pm — although you can frequently place an order outside these 'official' times.

Industrial sales calls tend to arrive (understandably) in the 2.30—4pm slot as well: remember that telex is a particularly useful medium as our telex is situated in the middle of the IM department.

We like to deal with customer service problems during the morning (10am-12.30pm) so that we have all afternoon to sort the problems out and 'catch the post'.

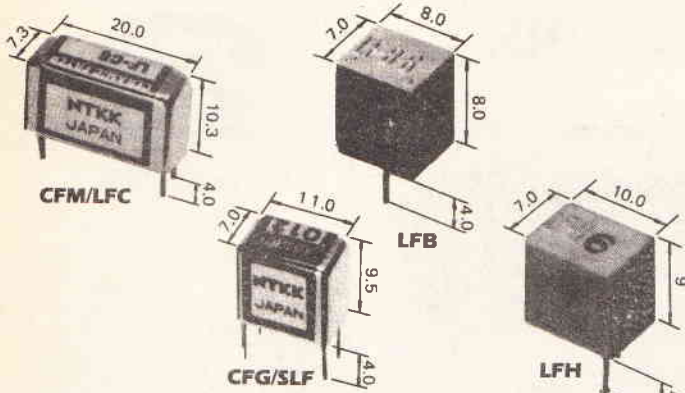
REWTEL provides on-line sales and stock enquiry facilities. (0277) 232628, a 300 baud modem and any one of a wide selection personal computers can be used to check stock and place orders, 24 hours a day, 365 days a year (less downtime!). Send an SAE marked 'REWTEL info' in the bottom left corner for more details.

ambit for communications components

The most comprehensive selection of coils, filters and components for all types of radio communications

CERAMIC FILTERS FOR 455kHz IFs

Ambit's range of ceramic filters cover most applications for communication and high quality broadcast reception. As far as we are aware, we hold the widest range of ceramic and crystal filter products anywhere in the world, and we will always do our best to assist if the type you want isn't immediately obvious from checking this section. We regret that we cannot generally assist in supplying replacements for imported equipment, unless the manufacturer's type number is available in addition to any 'house' numbers used to identify the parts.



CFM/LFC SERIES

A medium priced hermetically sealed ladder filter, suitable for most communications applications and high quality broadcast receiver equipment. Similar to the types used in receivers such as the FRG7.

Type No.	-6dB BW	-50dB BW	In/Out Impedance (k ohm)	Stock No	Price
CFM455H/LFC6	6	16	1.5	16-45520	5.20
CFM455G/LFC8	8	20	1.5	16-45521	5.20
CFM455F/LFC12	12	24	1.5	16-45522	5.20
CFM455E/LFC15	15	28	1.5	16-45523	5.20
CFM455D/LFC20	20	38	1.5	16-45524	5.20

A high performance filter, similar to those used in the R1000 and FRG7700. Ideal for all low cost SSB filter requirements, and suitable for upgrading existing equipment

CFM455J1	2.6kHz min	8kHz max	2k	16-45513	9.00
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CFG/SLF SERIES

A miniature high performance filter. Possibly the highest selectivity/size ratio available. Supplied in shield and hermetically sealed case, and recommended for use with designs involving the MC3357/9 and ULN3859 families, due to the excellent stopband performance.

Type No.	-6dB BW	-80dB BW	In/Out Impedance (k ohm)	Stock No	Price
CFG4551/SLFD4	4	10	1k5	16-45542	5.20
CFG455H/SLFD6	6	15	1k5	16-45542	5.20
CFG455G/SLFD8	8	18	1k5	16-45544	5.20
CFG455F/SLFD12	12	25	1k5	16-45546	5.20

LFB/LFH SERIES

Probably the most popular types of low cost ceramic ladder filter — found in most types of CB transceiver, and an increasing number of designs for commercial mobile radio systems. These filters possess excellent bandpass characteristics, although watch the stop band if you are not using them with some form of 'roofing' selectivity, such as a 2 or 4 pole crystal filter at 10.7MHz/10.695MHz. The impedances of these filters (and most of the other ladder series) is directly matched by such devices as the ULN3859, so extremely compact designs can be achieved at minimum cost. Miniature 455kHz filters. I/P and O/P impedance 2k.

NTK/Murata	-6dBW (Min)	-40dB (Max)	Stock No	1-24	25-99	100+
LFB4	4kHz	15kHz	16-45511	1.95	1.45	1.10
LFB6/CFU455H	6kHz	18kHz	16-45512	1.95	1.45	1.10
LFB8	8kHz	21kHz	16-45529	1.95	1.45	1.10
LFB10	10kHz	23kHz	16-45514	1.95	1.45	1.10
LFB12/CFU455F	12kHz	26kHz	16-45515	1.95	1.45	1.10
LFH6S/CFW455HT	6kHz	14kHz	16-45525	2.45	1.95	1.55
LFH8S	8kHz	18kHz	16-45526	2.45	1.95	1.55
LFH12S/CFW455FT	12kHz	22kHz	16-45528	2.45	1.95	1.55

CERAMIC RESONATORS

Low Cost, Small size alternative to Quartz Crystals

These resonators provide an excellent alternative to costly LF quartz crystals, and are especially suited to use with MPUs, rate generators, remote control systems, dial tone and dial pulse clocks etc. There are two basic types as with crystals — series and parallel resonant types. The majority of 'clock' applications will require the parallel resonant types (CRM), whereas 'bypass' and 'trap' circuits will usually call for the series (CFE) types.

Type	Frequency	Mode	Stock No	1-24	25-99	100+
CRM455	455kHz	parallel	16-45573	0.60	0.48	0.40
CRM460	455kHz	parallel	16-46073	0.60	0.48	0.40
CRM500A	500kHz	parallel	16-50073	0.60	0.48	0.40
CFE455	455kHz	series	16-45575	0.60	0.48	0.40
CRM560	560kHz	parallel	16-56074	0.60	0.48	0.40
CSA1.0MK	1000kHz	parallel	16-10003	0.94	0.84	0.76
455D	455kHz	NBFM Disc	16-15455	1.20	0.90	0.60

CRYSTAL FILTERS

We are pleased to be able to extend our range of crystal filters to include the popular 10.695MHz frequency that seems to be universally adopted in the first IF of CB receivers. A transplant of the 2 pole filter in place of the usual ceramic filter can perform the single most significant improvement in blocking and cross mod in most circuits and the popularity of the modification has spurred us to include an 8 pole version for the purist. The 90dB adjacent channel attenuation of the 8 pole series effectively removes all responsibility for blocking and IM related problems from the subsequent stages, and places emphasis on the RF and most crucially the mixers. The 10.7MHz 8 pole SSB filter is featured in the R&EW HF transceiver add-on for the R1000 or FRG7700 receivers and is at last managing to dispell the mystique that surrounds 9.0MHz.

2 POLE TYPES

Model	Centre Freq.(MHz)	Band Width(kHz)	Ripple (dB)	Stop Band (kHz)	Term Imp(kR)	Case	Stock No.	Price
10M15A	10.7	15(3dB)	0.5	±25.0(18dB)	3.0	FS12	20-10152	0.99
21M15A	21.0	15(3dB)	0.5	±25.0(17dB)	3.0	FS12	20-21152	3.45
10M08AA	10.695	8kHz	0.5	±25.0(18dB)	1.8	FS12	20-11152	3.49

8 POLE TYPES

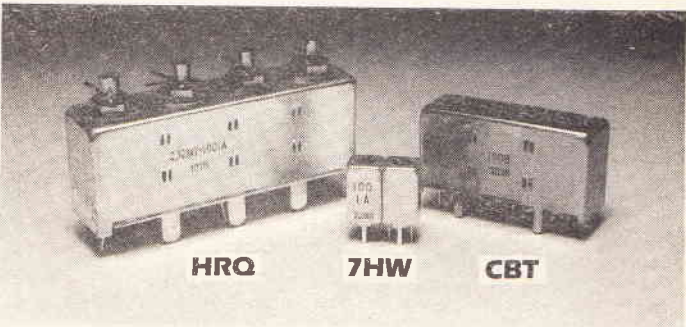
Model	Centre Freq.(MHz)	Band Width(kHz)	Ripple (dB)	Stop Band (kHz)	Term Imp(kR)	Case	Stock No.	Price
10M22D	10.7	2.2(6dB)	2.0	±2.4(60dB)	0.5	FS23	20-10028	17.20
10M8D	10.7	8(6dB)	2.0	±11.0(80dB)	3.0	FS22	20-10088	15.50
10M8DB	10.695	7(3dB)	2.0	±12.5(90dB)	3.3	FS22	20-11088	14.50
10M18D	10.7	15(6dB)	2.0	±20(80dB)	3.0	FS22	20-10158	14.50
21S08DA	21.4	7(3dB)	2.0	±12.5(90dB)	.850	S2	20-02108	15.65

Case Code

Case Code	L	W	H
FS22	18.5	12	15
FS23	23.0	12	15
S2	11.0	8.5	11.5

HELICAL FILTERS

Low cost filters for VHF/UHF



STOCK TYPES 7HW — 2 CHAMBER

Toko Part No. 7HW	Freq. MHz	Z in/out	1dB BW	Atten./MHz off centre	Ins loss (max)	Stock No.	Price
252MT1001A	435	50	12MHz	23dB/+30 29dB-30	4dB	17-10011	1.85
252MT1090A	470	50	8MHz	23dB-30 27dB-30	5dB	17-10901	1.85
252MN1127A	463	50	12MHz	15dB Min±30MHz	2dB	17-11271	2.25
252MN1111A	432	50	7MHz	18dB Min±30MHz	5dB	17-11111	2.25

STOCK TYPES HRQ — 4 CHAMBER

Toko Part No. HRQ	Freq. MHz	Z in/out	3dB BW	Atten./MHz off centre	Ins loss (max)	Stock No.	Price
232MT1001A	435	50	10MHz	28dB-15 31dB-15	4dB	17-10010	7.90
232MT1021A	470	50	6MHz	28dB-15 31dB-15	8dB	17-10210	7.90

STOCK TYPES CBW — 2 CHAMBER

Toko Part No. CBW	Freq. MHz	Z in/out	1dB BW	Atten./MHz off centre	Ins loss (max)	Stock No.	Price
271MT1006A	145	500	3.0MHz	25dB Min±15MHz	4.5dB	17-10062	3.15
271MT1007A	170	500	3.5MHz	20dB Min±15MHz	4.5dB	17-10072	3.15

STOCK TYPES CBT — 3 CHAMBER

Toko Part No. CBT	Freq. MHz	Z in/out	3dB BW	Atten./MHz off centre	Ins loss (max)	Stock No.	Price
272MT1006A	145	500	2.8MHz	25dB Min±6MHz	8dB	17-10063	3.15
272MT1007A	170	500	4.0MHz	30dB Min±6MHz	6dB	17-10073	3.15
272MT1019	160	500	3.5MHz	20dB Min±6MHz	6dB	17-10193	3.15
272MT1008	145	50	1.2MHz	30dB Min±6MHz	8dB	17-10083	3.15

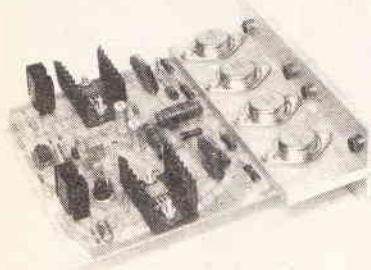
SEE THE COMPLETE CATALOGUE FOR DETAILS OF

- ★ Coaxial relays — PCB and connector types
- ★ TOKO IF transformers
- ★ TOKO block filters for video/radio
- ★ Fixed inductors
- ★ Quartz crystals

ambit for audio

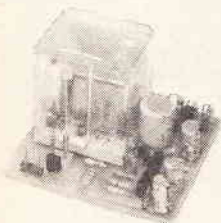
100W PA MODULE

All parts for the best 100W complementary amplifier yet published



Kit
41-00504 **36.48**
HEATSINK (2 required)
21-08035 **8.60**

LOUDSPEAKER/AMPLIFIER PROTECTION



Very substantial 20A relay driven by the multifarious HA12002 amplifier monitor IC. Protects against overload, temperature offset etc.

41-00505 **£8.39**

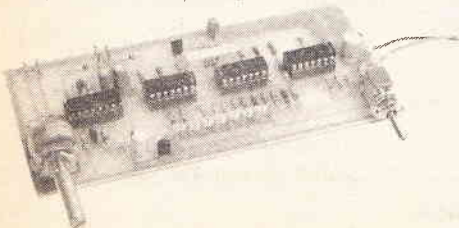
PSU — 250VA FOR PA

A multi primary toroid designed specifically for the above system with substantial reservoir capacitors

	Stock No.	Price
110/240V PRI 15-0-15V 42-0-42Vsec	57-07110	24.45
22000µF/63V	05-22400	7.84
200V PIV/ 25A Bridge Rectifier	90-00564	2.20

AUDIO LIMITER

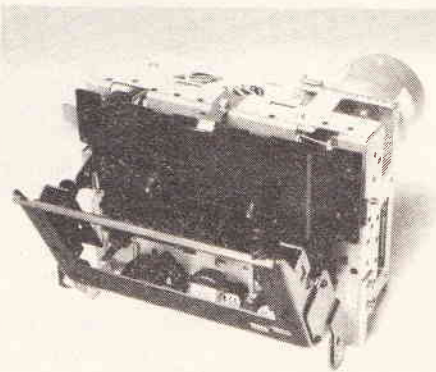
A high quality means of preventing amplifier overload in HiFi, PA or Broadcast systems.



Kit
41-00501 **£13.82**

ELECTRONIC CASSETTE

A fully solenoid operated cassette mechanism, featuring front loading and simple electronic control. Complete with Canon permalloy stereo head — although various others can be fitted if required. This is the current stock deck — OEM's can obtain details of the broader range available by contacting Ambit Industrial Marketing. Full specification and drawings on request, together with alternative head options for large volume users. Position counter available soon. See August R&W for details of logic drive circuit.

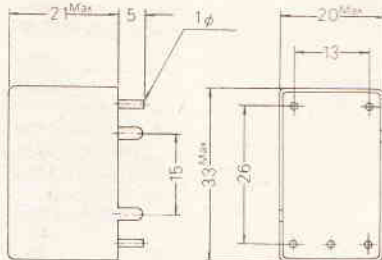


SPECIFICATION:

Rated Operating Voltage: Motor +12VDC ±10%, Solenoids -12V DC ±10%. **Installation:** Vertical or Horizontal. **Wow and Flutter:** >0.08% WRMS (>15)(Test Tape: TEAC MTT-111). **Spooling Time:** FF or REW >115 seconds (TDK DC-60). **Tape Speed:** 3,000Hz±2%. **Motor Consumption:** (Play, FF, REW)>100mA. **Heads - REC/REP:** Canon H3332-0202 (2 channel sendust). **Erase:** Canon H53211-02 (2 channel, double gap, metal capable)

Description	Stock No.	Price
TN3600 deck	72-03600	28.00
BAB43 Cassette deck control IC	61-00843	1.95
LB1288 Darlington Driver (for solenoids)	61-01288	1.35

TAPE OSCILLATOR BLOCK TBP23



Pre-aligned oscillator block for bias and erase use in cassette and tape decks. High stability push-pull oscillator, with shielded case.

SPECIFICATION:

Supply Voltage: 16V DC. **Current consumption:** <50mA. **Osc Frequency:** 100±5kHz. **Recording Bias Current:** 600µA per head. **Erase current:** 80mA. **Erase current distortion:** <0.6%. **Impedances:** **Erase Head:** 300R @50kHz. **Rec/Play Head:** 800R @1kHz. **Temperature Range:** -20° to +70°C.

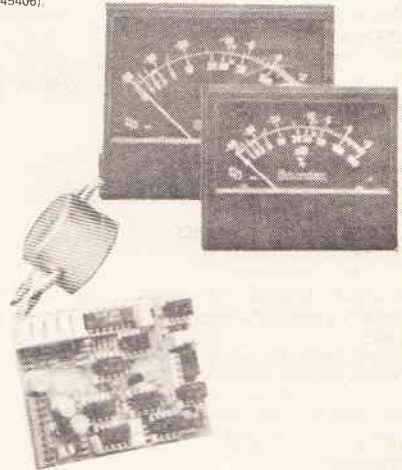
Type	Stock No.	Price
724BOR1018N	99-01018	2.75

PPM SYSTEMS

Professional ballistic sound measurement systems

PPM SYSTEMS TO DIN45406

The PPM 302 is a Meter Movement and Drive amplifier combination complete with 1:1 isolating transformer, forming a sophisticated peak programme meter system within BS 5428 type 1 and DIN 45406 specifications. The response time is exceptionally fast and the dynamic range -50 to 5dB. The drive card, incorporates a sharp cut off low pass filter, full wave rectifier, separate attack and decay time constants, and logarithmic meter drive amplifiers. The gain of the card is adjustable. The drive card and meter are sold as a pre-aligned pair and are issued with a calibration certificate. There are two meter sizes available and the size should be stated when ordering. PPM302/24 drive amp, card, balance transformer and size 24 meter (DIN45406), PPM302/34 drive amp, card, balance transformer and size 34 meter (DIN45406).



Type	Stock No.	Price
PPM302/24	50-30201	114.92
PPM302/34	50-30202	119.12

LOW COST PPM SYSTEMS

The PPM402 is a meter movement and Drive Amplifier card combination forming a cost effective peak programme meter of high quality and reliability. The driver consists of a variable sensitivity input stage, precision full-wave active rectifier and output stage with a transfer characteristic suitable for the meter scale. Each driver and meter is individually aligned to be within published data so that repeatability of response is guaranteed. In operation this means that peaks are not only captured, but also valued closely to what the ear may perceive. PPM402/24 drive amp, card with size 24 meter. PPM402/34 drive amp, card with size 34 meter. PPM402/K drive amp kit with size 24 meter.

Type	Stock No.	Price
PPM402/24	50-40201	55.13
PPM402/34	50-40202	59.73
PPM402/K	50-40203	45.98

DRIVE AMPLIFIERS

PPM 121 (ENCAPSULATED)

Features: ★ BS5428 compatibility ★ Small external component count ★ Maximum opportunity for user options. ★ Two-point line-up. ★ Small size 30 x 20 x 15mm ★ Wide supply variation tolerance. ★ Wide supply variation tolerance. ★ Low current consumption. The full wave rectifier, piece-wise processor and drive amplifiers, make this small module ideal for achieving Peak Programme Metering in a wide variety of applications. The module is sufficiently accurate to perform BS4297 and BS5428 processing with negligible thermal drift and wide supply tolerance. A minimum of external components are needed which allow dynamic and static parameters to be user-adjusted.

Type	Stock No.	Price
PPM121	50-00121	28.35

PPM 131 (CARD)

PPM 131 is a small, high quality meter drive amplifier, ideal for incorporation into mixers and other equipment where unbalanced signals are present. There is adequate gain to cope with non-standard levels. Power supplies present no problem to the PPM 131, since apart from being protected against reverse biasing, the amplifier may be operated from either single or dual rail power — the DV generator onboard can be linked in or out of use. Each PPM 131 leaves the Soundex factory having been aligned, both statically and ballistically, to the BS5428 specification and because only high stability close tolerance components are used, alignment is achieved in two steps.

Type	Stock No.	Price
PPM131	50-00131	36.75

Card to affix to meter

PPM 181 (CARD)

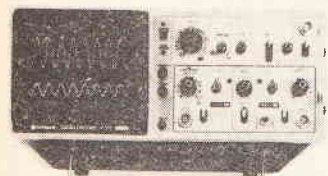
A high performance peak programme meter amplifier card of small size for mounting directly onto the rear studs of meter movements. The input is electronically balanced with a high input impedance and large common mode rejection. An unbalanced output is available for sum and difference measurement, where two PPM 181 cards are used as a stereo pair. The gain of the PPM 181 may be selected as unity (0dBm = 0dB indicated) or varied by appropriate linking. Realignment is a simple one pass procedure. The PPM 181 is supplied with 10 way edge connector, certificate of calibration and full data.

Type	Stock No.	Price
PPM181	50-00181	69.35

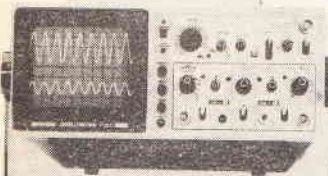
Card to affix to meter

ambit for low cost test gear and tools

HITACHI PORTABLE OSCILLOSCOPES



V212
DC to 20MHz
56-00212 **£305**



V222
DC to 20MHz
56-10222 **£350**



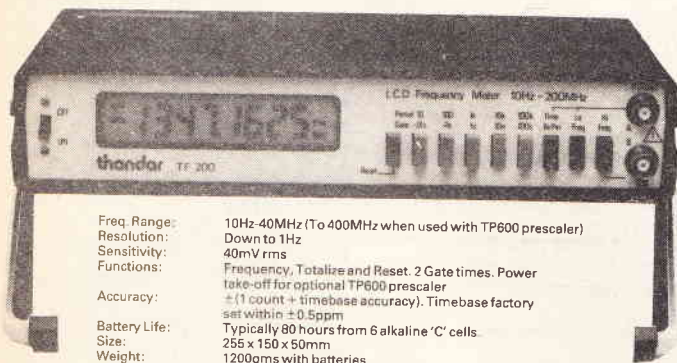
V422
56-00422 **£520**

LOW COST HIGH PERFORMANCE OSCILLOSCOPES

from one of the best known manufacturers in the industry

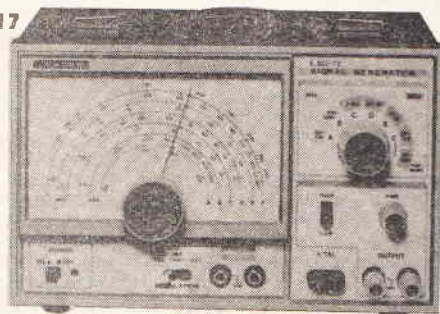
★ All above are dual beam, with built-in calibrator, probes etc.

THANDAR TF040 8 DIGIT LCD FREQUENCY METER



Freq. Range: 10Hz-40MHz (To 400MHz when used with TP600 prescaler)
Resolution: Down to 1Hz
Sensitivity: 40mV rms
Functions: Frequency, Totalize and Reset. 2 Gate times. Power take-off for optional TP600 prescaler
Accuracy: ±(1 count + timebase accuracy). Timebase factory set within ±0.5ppm
Battery Life: Typically 80 hours from 6 alkaline 'C' cells
Size: 255 x 150 x 50mm
Weight: 1200gms with batteries
Stock No.: 56-20000
Price: 145.00

RF GENERATOR LSG17



A stable wide-range generator for the hobbyist, service technician, schools, colleges, etc.

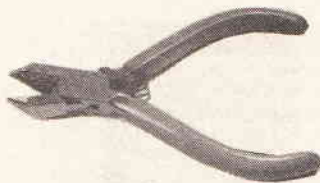
Freq. range: A/100kHz-300kHz, B/300kHz to 1MHz (Harmonics 96-450MHz) c/1MHz-3.5MHz, d/3.0MHz-11MHz, E/10MHz-35MHz, F/32MHz-150MHz
Accuracy: ±1.5% Output greater than 100mV (no load). Ext. xtal osc for 1 to 15MHz FT243 crystal
Power required: AC100, 115 or 230V 3VA
Size & Weight: 150(H) x 238(W) x 130(D)mm. 2.5kg approx.
Stock No.: 56-90017
Price: 71.00

'ENGINEER' RANGE PLIERS, CUTTERS

A range of low cost but superb quality handtools that feature best Japanese steel and box-joint construction (other than 54-30510). The cutter range includes slant and oblique types which are considerably better suited to trimming component leads through PCBs than standard diagonal types. We have no hesitation in recommending these as excellent value for money. Hardened bench engineers have been known to prefer these to other better known Swedish-made types costing twice as much.

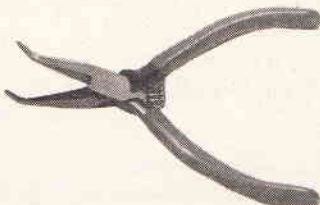
SLANT EDGE CUTTERS

Stock No. 54-50505 Price 5.30



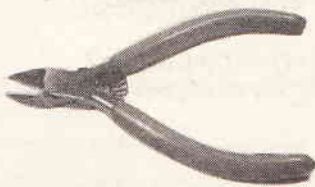
FLAT ANGLE NOSED PLIERS

Stock No. 54-30500 Price 5.30



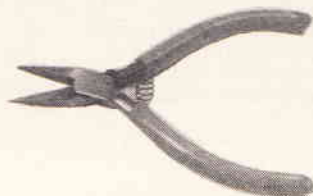
OBLIQUE CUTTERS

Stock No. 54-30506 Price 5.44



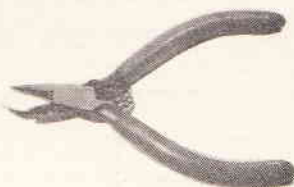
FLAT NOSED PLIERS

Stock No. 54-30501 Price 5.15



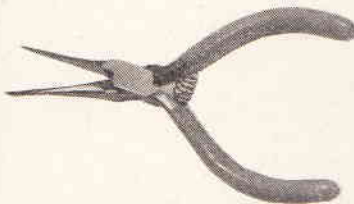
DIAGONAL CUTTERS

Stock No. 54-30507 Price 5.15



LONG TAPER NOSED PLIERS

Stock No. 54-30504 Price 5.44



LAP JOINT DIAGONAL CUTTERS

Stock No. 54-30510 Price 2.95



**MANY MORE
IN THE COMPLETE
CATALOGUE**

- SAME DAY DESPATCH WHENEVER POSSIBLE.
- PLEASE USE THE STOCK NO's - ORDERS WITHOUT MAY BE DELAYED.
- ONLY MANUFACTURER'S FIRST QUALITY GOODS.
- THE BROADEST RANGE , THE BEST PRICES.

ORDER FORM

Customer account No. if known

— Please check your last invoice. —

AMBIT INTERNATIONAL
 200, NORTH SERVICE ROAD
 BRENTWOOD
 ESSEX
 CM14 4SG

Tel: (0277) 230909
 Tlx: 995194

NAME & ADDRESS

POSTCODE

TELEPHONE:

PLEASE USE BLOCK CAPITALS

Qty	STOCK No.	PART No.	DESCRIPTION	Unit Price	SUB TOTAL
-					
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METHOD OF PAYMENT (please delete where appropriate)



SUB TOTAL

- CHEQUE
- POSTAL ORDER
- ACCESS or BARCLAYCARD
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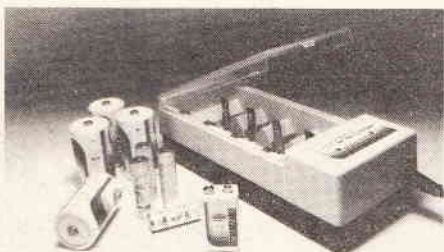


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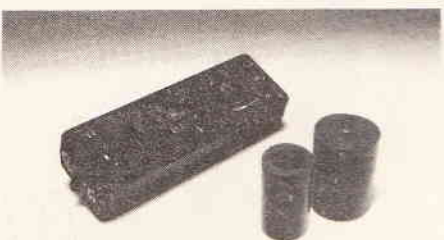


1 x 01-84054 PP3 NICAD = £ 3.70
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 AC Current; 0-200mA, 10A
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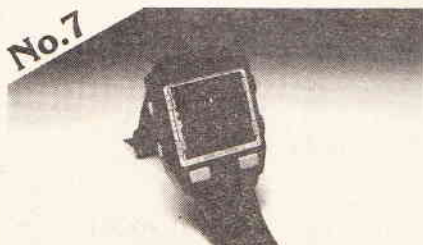
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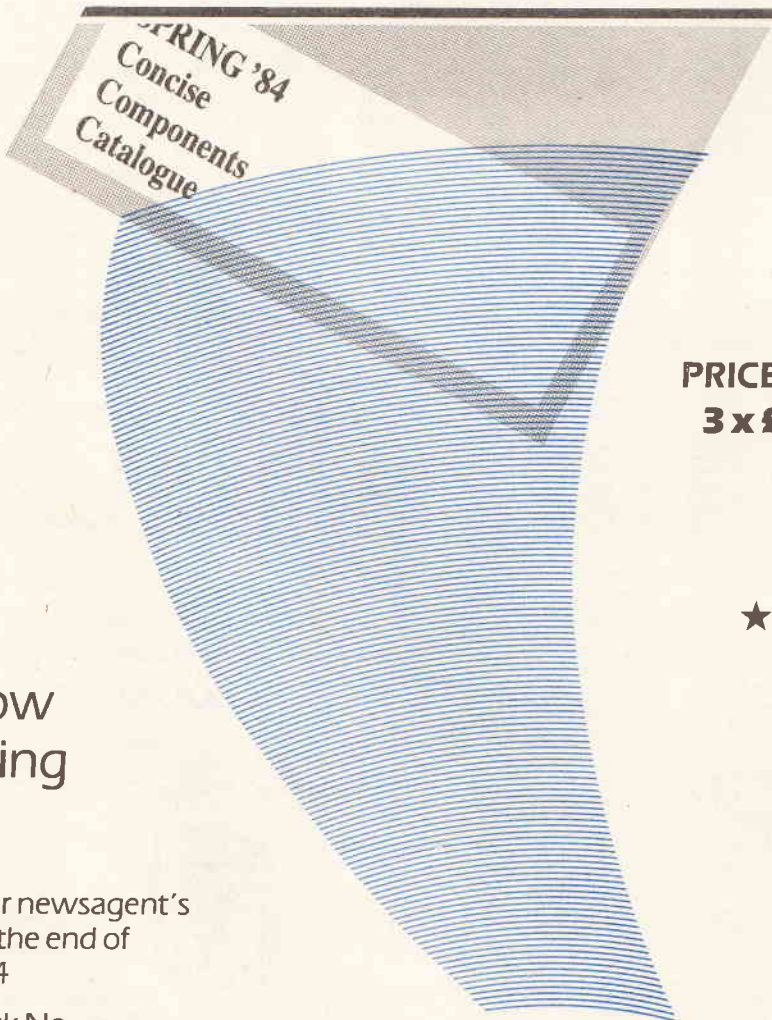
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We must apologise to our readers for missing out with our Winter edition — but we've been preparing something a little special to tempt you out of your Winter hibernation and back to the soldering iron.....

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e.g. 10mm plain cap, blue = 21-30015
28mm line cap, red = 21-30324

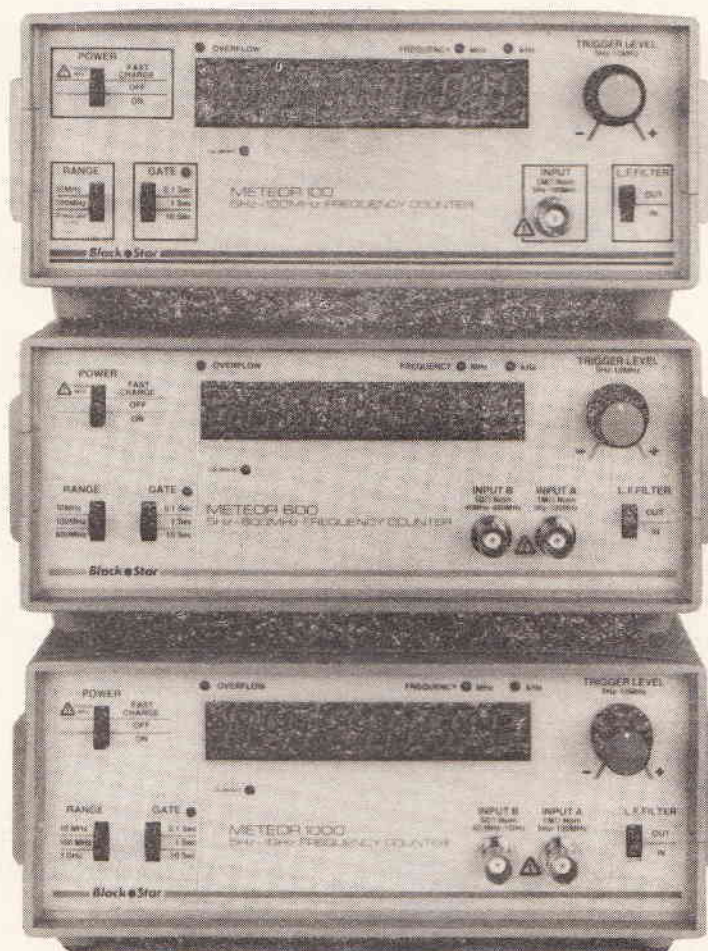
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Having been closely involved in a wide variety of OEM applications of their amp boards, Pantechnic became aware of numerous implementation problems often left untackled by other amp board manufacturers. These problems specifically of size and thermal efficiency became particularly aggravated at high powers and considerably lengthened OEM product development time.

By including thermal design in the totality of board design it has been possible to reduce the size of the electronics, and increase the efficiency of the transistor to heatsink thermal circuit. The combined effect of this has been to dramatically increase the volumetric efficiency of the amplifier/heatsink assembly. The **SYSTEM** Amp offers 1.2KW of power in a space of 180mm x 102mm x 77mm, excluding PSU and Fan.

The basis of this considerable advance is the **PANTECH 74 Heat Exchanger**, newly designed and manufactured by us. By eliminating the laminar air flow found in conventional, extruded heat sinks, heat transfer to the environment is greatly enhanced.

The flexibility of the 1.2KW amp stems from its division into 4 potentially separate amplifiers of 300W each (downrateable with cost savings to 150W). These can be paralleled, increasing current capability or seriesed (bridged in pairs) doubling voltage capability. In consequence a large variety of amplifier/load strategies can be implemented.

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PFA/HV	36.04	200-300W	4, 8, 8Ω, 16Ω	5dB dynamic headroom Drives 70V line direct.
*PFA500	45.22 55.33	250-600W	2, 4, 8, 16	25A cont. output current. mounted on type 74 Heat Exchanger (see below).

*The power output of these amplifiers can be increased by approx 15% with no diminution in quality by adding PSU102 (£7.61) to your existing power supply.

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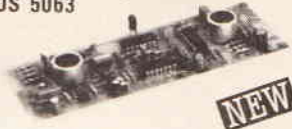
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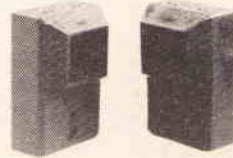


- Adjustable range from 5-25ft.

This popular low cost ultrasonic detector is already used in a wide range of applications from intruder detectors to automatic light switches and door opening equipment, featuring 2 LED indicators for ease of setting up, the unit represents outstanding value at

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INFRA-RED SYSTEM IR 1470



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Provides stabilised 12V output at 85mA and contains a relay with 3 amp contacts. The unit is designed to operate with up to 2 ultrasonic units or 1 infra-red unit IR 1470. Price **£4.25 + V.A.T.**

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5 1/2" HORN SPEAKER HS 588

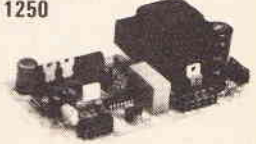
This weather-proof horn speaker provides extremely high sound pressure levels (110db at 2 metres) when used with the CA 1250, PS 1865 or SL 157. Price **£4.95 + V.A.T.**

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- Separate relay contacts for switching external loads
- Test loop facility

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SIREN & POWER SUPPLY MODULE PSL 1865



A complete siren and power supply module which is capable of providing sound levels of 110db at 2 metres when used with a horn speaker. In addition, the unit provides a stabilised 12V output up to 100mA. A switching relay is also included so that the unit may be used in conjunction with the US 5063 or US 4012 to form a complete alarm.

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LM1305 2.75	LM1305 2.75	LM1305 2.75	TAA522 2.47	7400 19p	74LS00 19p	74LS399 1.59	4016 32p	75LS289 3.25	75LS289 3.25	75LS289 3.25	75LS289 3.25	75LS289 3.25	75LS289 3.25	75LS289 3.25	75LS289 3.25	75LS289 3.25	75LS289 3.25

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AUDIO DESIGN

Few areas of electronics have accumulated as much superstition and hype as the design of power amplifiers — here is John Linsley Hood's attempt to cut through the muddle.

A considerable amount of mystique surrounds the whole field of audio amplifier design, particularly in regard to the part which actually delivers electrical power to the loudspeakers, and a vast amount of effort is spent in laboratories, listening rooms and editorial offices in sorting the good from the not-so-good. How much of this mystique is justified is a speculative question, a source of pleasure for those whose efforts have been received with acclaim, and a source of indignation for those whose designs have been ignored by the cognoscenti or impugned by the pundits.

My own feelings in this matter, particularly in respect of the hi-fi devotees, are highly ambivalent. On the one hand, I am convinced that much of stock in trade of the hi-fi journals, their 'subjective' reviewers, and the manufacturers and dealers who follow in the train of their approval, is built upon the identification and exaggeration of differences which are, in reality, fairly small. On the other hand, I know that there are sound differences between differing designs, some of which are easy to live with and render their inputs to the listener in a pleasing — and sometimes exciting — light, others have the capability to make everything they handle sound rather drab and second-rate, and others may appear fine at first hearing and yet, after a day or two, make one not wish to listen further.

Some of this is simply a matter of incompatibility between the separate parts of the audio system: I still remember, very clearly, paying a visit to a hi-fi fanatic of my temporary acquaintance, who had spent many thousands of pounds in assembling a set of gear which included all the most expensive and exotic bits of hardware that had received rave reviews in the magazines. His wife would not stay in the same room with it. After listening to it for half an hour, I didn't blame her. So one of the basic requirements of an audio power amplifier must be that it should be highly tolerant of the type of LS load applied to it.

Other components of the sound quality characteristics of the power amplifier relate to quite clearly definable design aspects, which one hopes that the designer will have given due thought to. Yet other contributing factors undoubtedly reside in a grey area of technology as yet not very clearly defined, where one may more surely say that this or that is a good thing to do — because one knows from experience that this is the case — but one cannot be so certain that something else, as yet untried, will be equally good, or give sound engineering reasons for this belief.

So — this is the scene; now to the engineering.

Output Power

Because of the nature of the sensitivity of the human ear, and of the physical principles of acoustics on which hearing is based, doubling the amount of electrical power fed to a loudspeaker does not make the resultant sound appear twice as loud. In reality, this is a

logarithmic relationship, in which apparent increases in sound loudness are related to power by the equation $W = k \cdot \log_{10} P_2/P_1$. While precision in this field is difficult because of the subjective nature of the thing being measured, and because apparent loudness is related to frequency anyway, one can say, roughly, that 3W, 30W and 300W are increments in amplifier power which would correspond to doublings in sound loudness at maximum volume. One can see from this that some very big steps in amplifier power are needed to get significant gains in sound level. The converse is also true, that microscopic amounts of sound power, like the buzzing of a fly's wings, or the LS output from the noise voltage of a well designed low-noise amplifier, are still quite audible!

As we have seen earlier, power output is related to output (RMS) voltage and load impedance by the equation $P = V^2/R$ or $P = I^2R$ in the case of output current. If an output of 100W is required into an LS load of a nominal 8 ohm impedance, an RMS output voltage swing of $\sqrt{800}$ (28.28 V) is required. This corresponds to a peak-to-peak voltage swing of 80 V. Allowing for voltage drops in the various output stage components a potential between +ve and -ve HT lines of 120 V is probably needed. Now, let us suppose that the LS impedance drops to 2 ohms at 15 kHz. 100 W will then correspond to a peak current of $\sqrt{50} \times \sqrt{2}$ amps, or 10 A. (Fortunately we don't have to cater for a peak-to-peak current!) So, our amplifier, to meet this spec. with this load, would need to be able to deliver 28.82 V RMS and 10 A peak current, but not simultaneously, normally. Powerful amplifiers need big, and expensive, power supplies. They also need transistors and capacitors which are capable of withstanding these high working voltages. Apart from this, and the bigger heat sinks, they are not much different in design from their smaller brothers.

Power Bandwidth

The audio spectrum is assumed to lie between 20 Hz and 20 kHz. With average listening rooms, average good quality LS systems, average listeners, and averagely good quality programme material, 45 Hz — 15 kHz is a more realistic assessment. Happily, there isn't much programme energy in the part of the audio spectrum above 10 kHz, or we wouldn't stay around very long to listen to it, so — being realistic — we don't need to cater for maximum power output in this region unless the equipment is going to be reviewed. There is also not much VLF output from either programme material or LS units. Unfortunately, in this case, if the amplifier cannot operate well below 30-40 Hz it will sound 'thin', and will probably overload on spurious signal inputs (record rumble and the like) which is disastrous sonically.

Some of the more acute listeners can undoubtedly hear the difference when HF response is curtailed, even though this is above their ear's frequency response — because of the absence of beat-note effects due to the interaction of high frequency sounds within the non-

linearities of their own ears. A better HF response may not make things sound better, but it can make them sound different.

This is where the first of the needs to compromise occurs. With typical power junction transistors, which are fairly sluggish devices, increased HF power bandwidth can only be obtained at the expense of loop stability in a negative feedback amplifier (though feed-forward systems avoid this snag). If loop stability is poor, the amplifier transient response is bad, and this can introduce some pretty drastic distortions into pulse type signals, such as drum beats or cymbal clashes. An amplifier with a good loop stability is usually much more pleasant to listen to, and will certainly be less fussy about the LS load characteristics.

Negative Feedback And Loop Stability

Negative feedback — the instantaneous electronic comparison between the signal at the output of an amplifier, and the signal at its input, and the generation of a corrective adjustment to the effective input signal to make sure that these input and output signals are closely identical — remains the major tool in the hands of the circuit designer. However, there are snags!

We have seen earlier in this series that we need to use enough NFB. Too little may just make matters worse, by substituting less pleasant forms of distortion for the ones we have reduced. We also need to make sure that our use of NFB does not make the whole system unstable, and this is particularly the case for audio power amplifiers which have to drive LS loads, since these are notoriously complex in their impedance and delayed response characteristics. It is also essential to remember that a feedback path is just what its name suggests, a means by which signal components, both wanted and unwanted, can be fed back from the LS load to the input of the amplifier. Since LS units can and do generate electrical signals of their own (as a result of internal cabinet echoes, and as a consequence of inadequately damped reflections along the LS diaphragm) we need to watch this point.

With regard to loop stability, this field was investigated by Bode and Nyquist very many years ago, in respect of the parallel field of closed-loop servomechanisms. Personally, I find the Bode diagram, of Fig. 1, the easiest to follow and to explain. In this diagram, the gain and phase-shift of the amplifier is shown simultaneously as a function of frequency. If the amplifier has a gain of 1 (or more) at a frequency where the feedback is in phase with the input (an NFB phase

shift of 180°) it will oscillate. The reason for this is simple, it is that the feedback path is itself providing an input signal of the right size and phase to generate the actual output, without the need for any other input signal at all! If the gain is more than unity at this frequency, the signal output will continue to increase until some other effect, such as clipping, reduces the gain to unity.

Unfortunately, it isn't sufficient merely to ensure that the amplifier doesn't oscillate on load, there must be an adequate margin of gain, or phase, at the -180° , or unity gain, points to make sure that the amplifier isn't triggered into some form of misbehaviour during transients in the input signal, or during temporary overload. In particular, the 'settling time', the time which is required following a sudden input voltage excursion before the system settles at the new level, depends solely on the system speed and stability margin, as shown in Fig. 2. I would very much like reviewers of audio amps. to measure, and quote, this value for a square-wave, or step input, with a real live LS load, since this is one of the areas where the pursuit of low THD values, at the top end of the audio spectrum, can lead to circuit design characteristics which are bad for the transient handling qualities of the amplifier, and may make it very fussy about the LS units with which it is used. As a comment on this, it does seem pointless to try to reduce 0.1% THD at 20 kHz, which is inaudible, and swamped by the distortions on the input signal, (if there is any, at this frequency) to 0.01% THD, which is just as inaudible, if the price one has to pay is a very bad transient response, and some 20-50% distortion on transient signals — which is very clearly audible!

By and large, in a typical audio amplifier, the major factor which dominates the gain and HF phase-shift characteristics is the relative sluggishness of the output transistors. The faster the response of these, the easier it is to design a good, stable, amp. The snag is that fast output junction transistors are also more fragile, and need more restrictive protection circuitry to prevent them from damage in use. This in turn makes the amp. less good at driving low impedance LS loads, and so on . . . Valves, of course, would be faster, were it not that a very sluggish and awkward output transformer is then needed. The answer, and a virtually complete one too, is to use power MOSFETs. Some of the recent ones of this type have a virtually instantaneous response, and are more linear in their characteristics than either valves or junction transistors. They too have snags, of which the

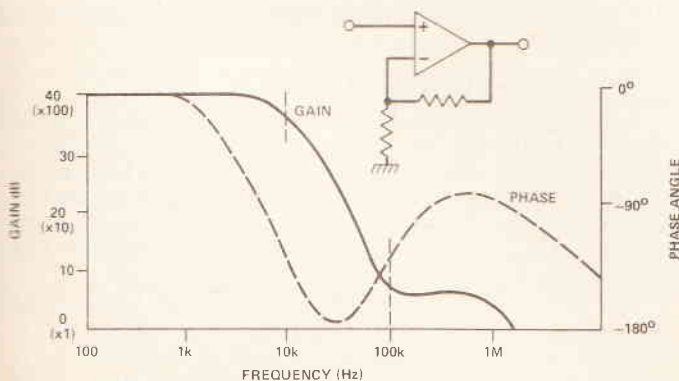


Fig. 1 Gain/phase or Bode diagram for conditionally stable feed-back amplifier (a change of load might make this amplifier oscillate at 30-50 kHz).

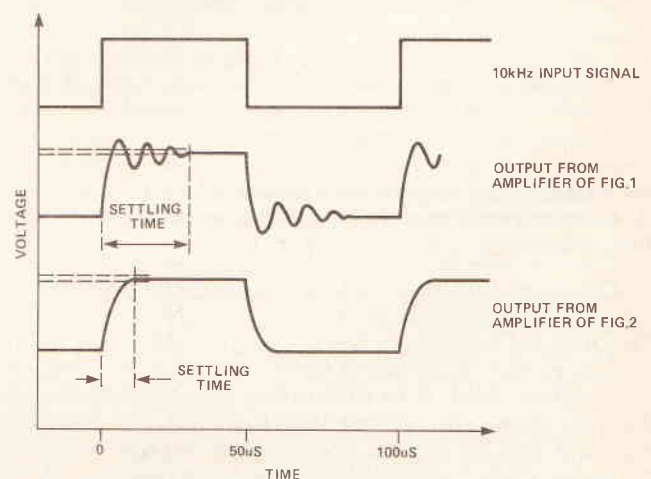


Fig. 2 Influence of gain and phase margins of NFB amplifiers and settling time.

main one is that they are fussy about the phase characteristics of their loads, but there is a simple design answer to this. So, with power MOSFETs, and some reasonably straightforward design, it is practicable to design audio power amps. which are a good ten times better, technically, than their possible forerunners.

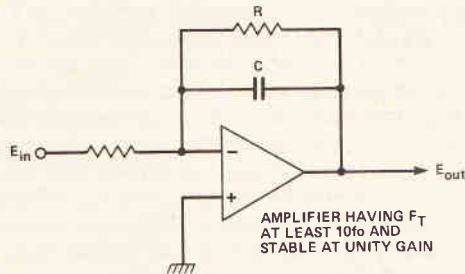


Fig. 3 Feedback amplifier having good gain and phase margins.

Distortion — And NFB

We have seen earlier that not all distortion types are equal in their unpleasing effects, and also that the character of a distortion can be greatly influenced by the relative phases of the signal components (clipping and crossover types differ mainly in the relative phase of the discontinuity, but sound very different). This effect has relevance to the behaviour of multi-driver LS systems, which can jumble up the phases of the signal (= time of arrival to the ear) and thereby alter the nature of amplifier nasties. So our efforts in the design exercise should be aimed at removing components of distortion which can be so transformed.

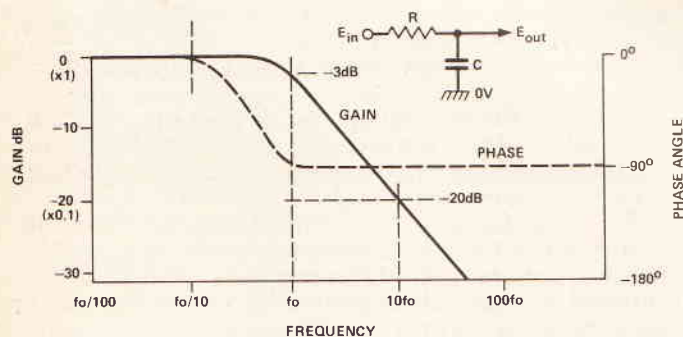


Fig. 4 Gain/phase diagram for a simple RC attenuator; the characteristics of the amplifier in Fig. 2 would be similar to this.

Obviously it is helpful if we can keep the distortion of the amplifier as low as possible before NFB is applied, in that low NFB leads to better loop stability. A useful design yardstick, cribbed from the servo-mechanism engineering field, is to determine the 'time constants' (the RC integrator values which would, for example, simulate the HF roll-off characteristics of the components or circuit elements being investigated) of the several bits of the circuit, and then make one of these — perhaps deliberately added — ten times the size of the rest. This isn't quite as arbitrary as it seems, since if we wish to end up with the fairly ideal Bode diagram for the

amplifier shown in Fig. 3, we must remember that a phase shift due to an RC element begins one decade, in frequency, below the -3dB 'turn-over' point of that network, shown in Fig. 4. In this way, the system will tend to behave as though it had only a single phase-shifting component.

A further useful design approach is to try to design the system so that there are not more than two signal handling 'gain' stages within the NFB loop, using more loops if necessary. This approach isn't easily possible with power amps. so other approaches may be necessary, including the useful phase-lead generating 'step network'. However, one can always put in an internal NFB loop, operating only at HF (the place where in transistorised amplifiers trouble is likely to arise) and including only two gain stages. This is a helpful technique which leads to good-sounding amplifiers.

The aim of the designer should be to produce an amplifier in which the harmonic distortion is as low as possible, and the gain bandwidth as high as possible, before the application of any NFB, so that the NFB can be used mainly to control and stabilise the gain and output impedance characteristics, rather than as a way of lowering the distortion.

So far as the feedback path itself is concerned, it is probably better not to employ a parallel HF compensation capacitor across the NFB resistor, in that this can make the amplifier sound less well on some LS units. It is also helpful in the task of making the amplifier as widely load-compatible as possible, if a small resistor, in the range $0.15\text{--}0.33\ \Omega$, is connected in the output circuit of the amp. to act as the input limb of an attenuator, against the much lower output impedance of the amplifier itself, to assist in attenuating signals originating in the LS units themselves, and preventing these from getting back to the amplifier inputs.

A final thought, with regard to amplifier 'sound', G. King some years ago pointed out that the human ear is not a very good judge of performance in respect of distortion, in that of a number of randomly chosen people, all reasonably competent judges of sound quality, either preferred the presence of some 0.3% even order harmonic distortion (deliberately added after the signal sources) or had no specific preference. Similar work has been done by other investigators. This tends to cast doubt on the value of such judgements, where the listener may actually prefer an inferior performance, because of attractive colouration added to the sound, and think the equipment is therefore better (i.e. more faithful to the original output). One cannot, unfortunately, design for this — and whatever its sonic merits, distortion will always make clear sounds somewhat more muddled.

A Practical Design Approach

Earlier in this series, I referred to the need to prevent intrusion of signals from the supply lines into the signal path, and to the ways of linearising gain stages. I have also urged the quality benefits which can be gained by the use of stabilised power supply lines, in a previous article², so let us now add this information together in a practical design exercise.

My preference for power MOSFETs as the output devices is definite, but not just as simple source-followers where they require an output inductor in the LS lead in order to prevent VHF oscillation due to the devices own small source lead inductance. If the power MOSFET is used in combination with a bipolar small-signal transistor, in the output stage layout shown in Fig. 6, this small inelegance can be avoided, without

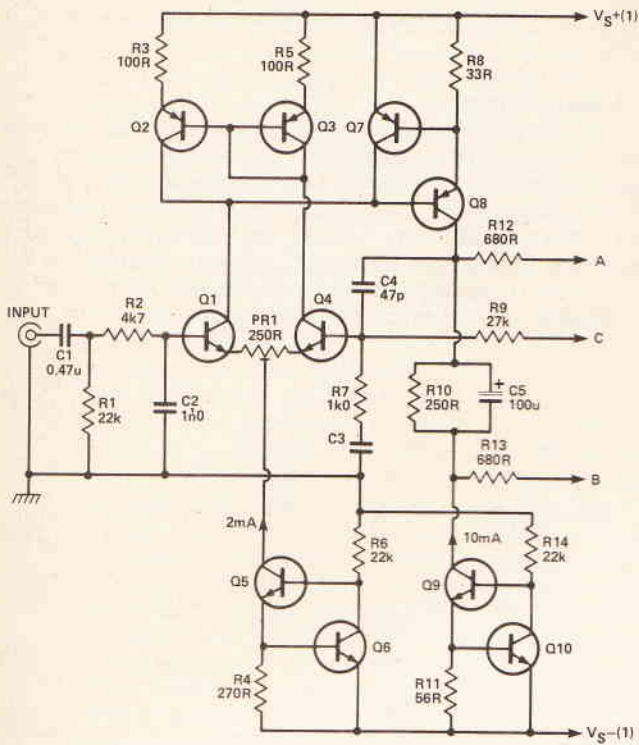


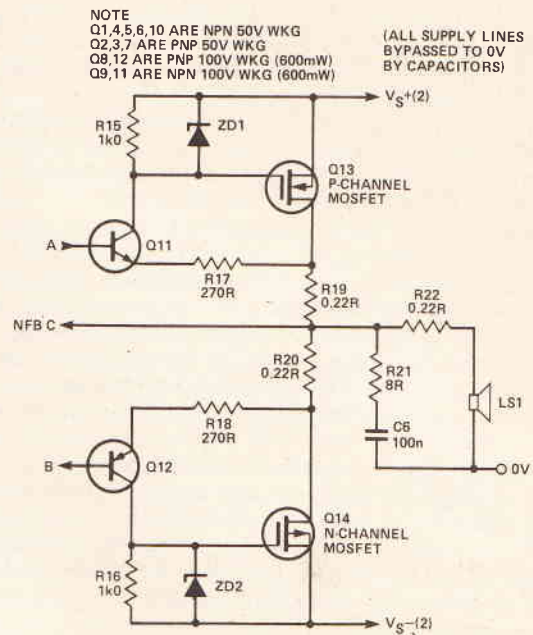
Fig. 5 Power amp. driver stage.

degradation of the fast response of the Mosfet. The only necessary device protection can then be an output circuit fuse, or better still, a current limited DC power supply, since the circuit resistance of fuse-holders (and LS connectors) is finite and non-linear!

A typical small signal voltage amplifier to drive this output stage is shown in Fig. 5. Because small-signal bipolar transistors are cheap, I have been fairly lavish in my use of these, where they can confer some practical benefit in the operation of the circuit. Starting from the beginning, there is an input DC isolation capacitor C1, and a resistor R1 to define the '0V' DC level of the input. R2 and C2 are an HF roll-off circuit, to prevent very fast HF transients being applied to the power amplifier. A time constant of $4.7 \mu\text{s}$ ($4\text{k}\Omega$ and 1nF) will give an HF -3dB point at 33kHz , which is adequately outside the audio band, but not so high as to be ineffective.

In order to preserve the DC symmetry of the input stage, which is a long tailed pair in the interests of low distortion, the total resistance path should be the same for Q1 and Q4 bases, which fixes R1 at $22\text{k}\Omega$. Q5 and Q6 are a two-transistor constant-current source, of the kind we have already met, with the value of R4 chosen to give a collector current of 1mA through each of the input transistors. PR1 is a preset trimmer which allows the DC output level of the power amp. to be adjusted precisely to 0V . Because the Q5, Q6 type of constant-current source has a very high dynamic resistance, it helps to prevent unwanted AC rubbish from getting into the input circuit from the $-ve$ supply line.

I have chosen to use a simple current mirror, Q2 and Q3, as the load for the input long-tailed pair, in order to combine the signals from the two input transistors and optimise the input stage gain. From this, the signal is fed to the second stage amplifier — a medium power PNP transistor in the interests of gain linearity — again loaded



NOTE
Q1,4,5,6,10 ARE NPN 50V WKG
Q2,3,7 ARE PNP 50V WKG
Q8,12 ARE PNP 100V WKG (600mW)
Q9,11 ARE NPN 100V WKG (600mW)

(ALL SUPPLY LINES
BYPASSED TO 0V
BY CAPACITORS)

Fig. 6 MOSFET output stage.

by a two transistor constant-current source, to ensure high AC gain and low distortion (if the current change through Q8 were zero, the distortion due to Q8 would also be zero). In this case, the value of R11 is chosen to give a collector current of 10mA , in order to lessen the effect of the variable drive current into the output stage input transistors, and in order to push the maximum slewing rate possible with C4 up to a high value.

R11, bypassed by C5, provides the necessary 1.2V potential drop to bias the output stage to a 100mA quiescent current.

Under overload conditions, Q9 and Q10 limit the current which can be drawn from the $-ve$ line to 10mA . Q7 and Q8 provide a similar anti-destruction protective function in respect of Q8 and the $+ve$ line.

R9, R7 and C3 provide the negative feedback path from the output stage to stabilise the AC gain to 27 , which is a convenient value since it allows maximum output (in this case 50W) from a '0VU' (0.77V RMS) input signal level. C4 provides HF stabilisation by means of an internal HF NFB loop just enclosing the two gain stages Q1/4 and Q8, which gives a good, well-damped, transient response, especially under the critical reactive load conditions. LS units most definitely do not behave like 8ohm load resistances!

R12 and R13 serve the useful function of preventing temporary latch-up if the amplifier is driven into clipping; in their absence clicks and bangs are prolonged, and sound louder. Also, clipping will sound more objectionable without them.

The output stage which will join on to this amplifier, and which I have shown in Fig. 6, with component numbers appropriately labelled to follow on, is unusual in that it uses the MOSFETs in a compound emitter follower configuration, with Q11 and Q12 as the input devices. Because the LS load is then connected to the

drains of the power MOSFETs, the need for the series output inductor is removed. Excess voltage across the gate-source junctions of the MOSFETs is prevented by ZD1 and ZD2, while R15/17 and R16/18 limit the AC gain of the output stage to 5.

R22 is the resistor which attenuates signals returned from the LS unit, and R21/C6 is the so-called Zobel network which prevents the output stage seeing an open-circuit at HF if the LS unit is disconnected.

I have labelled the DC supplies to the AC gain and output stages VS+(1) and VS+(2), and VS-(1) and VS-(2). This is because it is then possible, and advantageous, to operate these from two separate DC supply sources, which prevents intrusion of high powered nasties from the output stage supply lines into the sensitive earlier stage circuitry. This gives most of the advantages of a system operated from stabilised DC supplies, but at a much lower cost. Also, if one wishes, one can operate the gain stage (Fig. 5) from a stabilised source — after all, one has to supply only 12 mA per channel, which doesn't make it too dear — and then operate the output stage from really large, low equivalent series resistance, DC supply electrolytics, and gain the benefits of both, though one would then need fuse protection in the LS lines.

So, this is how one gathers together the requirements in the design of an audio amplifier. Now while this is a very good amplifier, of the best modern standards and with an excellent technical and audible performance, I am not, at this stage, going to fill in all the small details, power supplies, PCB and component layout, etc, because this amplifier is strictly conventional in its design approach, and we can do some rather more crafty tricks in this type of design, to give us just a little extra. So, regard this as a design exercise, the sort of thing which the circuit designer of some amplifier manufacturing firm will do when his boss tells him they need a new up-market design to go with the magnificent advertising promotional blurb, which the Ad. agency have already come out with. (Though, in reality, the designer will always have to do a bit of 'fine tuning' to the circuit, to make sure that it is as good as possible in all the various conflicting requirements of the system.)

I will show a final, 'improved', version of this, with a very high quality preamplifier — again, already outlined in form in a preceding part of this series — and appropriate power supplies, in a later article. Meanwhile, may I round off this part of the series with a look at some of the possible 'amplifier types'.

Class Distinctions?

Although, as I have indicated above, I have an ambivalent attitude to the razzmatazz of the hi-fi scene, as an audio circuit designer I cannot escape from contact with it, and I read with interest, surprise, concern or dismay, the comments and thoughts of my peers in this field. A large aspect of this, which has been continuously explored, and argued about, ever since transistors appeared on the scene, has been the debate valves vs. transistors, and class A vs. class-AB (or w.h.y.). Since I originally stuck my nose into this field as the author of a simple class-A design (which I valued because it was simple, rather than because it was class-A and which is as good as any amplifier I have designed or obtained from other sources since then) I cannot simply say, with my friend Reg Williamson, that class-A is the lazy man's solution, a simple 'sweeping of design problems under the carpet'.

I have, in consequence both of my original involvement and the subsequent, continuing debate, spent

many hours in thought and experiment on these points, and have come slowly to conclusions which I am prepared to defend.

Valve Amps

These are not usually very good, technically. Even the best of them will not compare well, in performance, with a good transistor unit. However, they do have some useful advantages. The first of these is that they are pretty well unburstable; the second is that they overload gracefully, with a rounded-off clipping, which allows the loud-noise brigade to drive them closer to the permanent clipping level without driving the dog mad. This

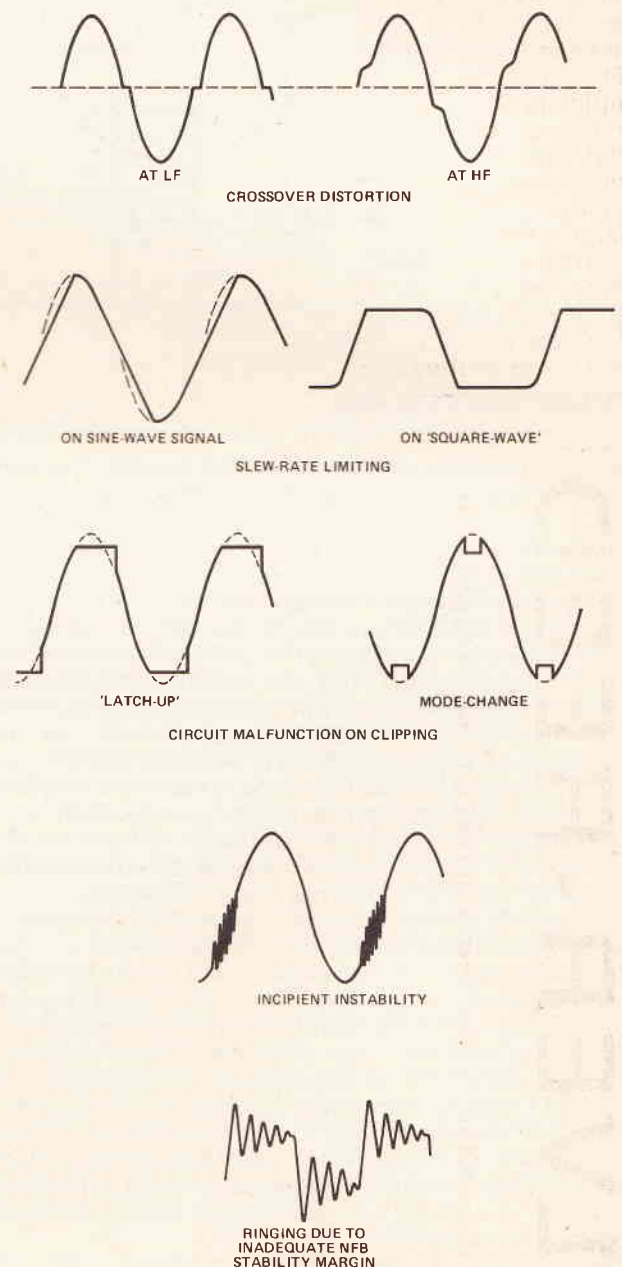


Fig. 7 Oscilloscope waveforms of some power amplifier circuit malfunctions.

allows the legitimate claim that they sound 'louder' for the same wattage. However, distorted sounds also sound louder than undistorted ones. The third advantage is that their distortion products, of which there are usually quite a lot, are of a kind to which the ear does not object too strongly. Fourthly, because they don't usually use much NFB (they can't because of the o/p transformer phase shifts) they are tolerant of LS loads. Finally, they look pretty, and make the Joneses jealous. The snags start with the price!

If one wants to, one can build 'soft clipping' into the preamp. for one hundredth of the price.

Class-A vs. Class-B

If one must use junction transistors, there is little doubt that they will work better in class-A (where the quiescent current is that which is needed for full output). They will have a better, and more uniform HF response and much lower distortion for the same amount of NFB — and hence a better transient response. Class 'A' amplifiers do, however, chuck out an awful lot of heat if any large amount of power is needed. Remember that at 20% efficiency a 100W/channel amp. would generate 1kW of heat, and need to get rid of this with the amp. at less than 100°C. If you can be content with 10W/channel, then class-A is an excellent choice.

So far as class-B (or more strictly AB) is concerned, where the amplifier operates at a quiescent current significantly lower than the operating one, cross-over distortion is inevitably present where one output device hands over to the other. Good circuit design, and the

judicious use of adequate NFB, will reduce this to less than the background noise level, especially if the output devices are power MOSFETs, rather than the more sluggish junction devices whose limitations begin to show in the 10-20kHz region. I do not, honestly, think that the differences between these types are anywhere near as big as the differences between different FM channels, or between different pressings of the same LP disc.

Feed-forward techniques, as in the 'Quad' current dumping amplifier, where a small, low powered class-A amplifier is used to fill in the missing bits in a straight class-B output stage, give results which are comparable to other good design approaches using similar output devices. Variations in the feed-forward technique, which is, itself, of considerable age, have allowed the Japanese publicity agents scope for much exaggeration.

For the record, I have shown in Fig. 7, the 'scope waveforms of some typical power amplifier defects, which, one hopes, the designer will have removed before manufacture starts.

In my next part of this series I propose to look at the field to tape recoding and cassette systems, an area which has developed enormously in the past few years.

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2. Linsley Hood, J. L., Electronics Today International, May 1983, pp 18-22.

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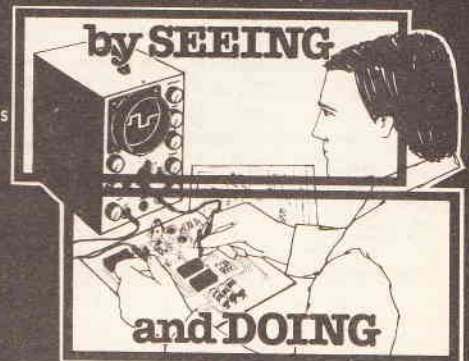
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TECH TIPS

Semi-Switchless Switch

Ian Sherlock
Preston

Designed to alleviate the persistent use of a wall light switch, this circuit could also be of use in households with elderly or disabled members. The circuit turns on the light when anyone enters the room (which must have a single entrance), counts the number of people entering or leaving, then turns off the light again when the room is empty.

The phototransistors each give a positive-going long pulse when the light to them is blocked; they should be about 5 to 10 cm apart, so that

both beams are cut for much of the period of time it takes someone to enter. These pulses are amplified by Q1 and 2 and IC1a and b.

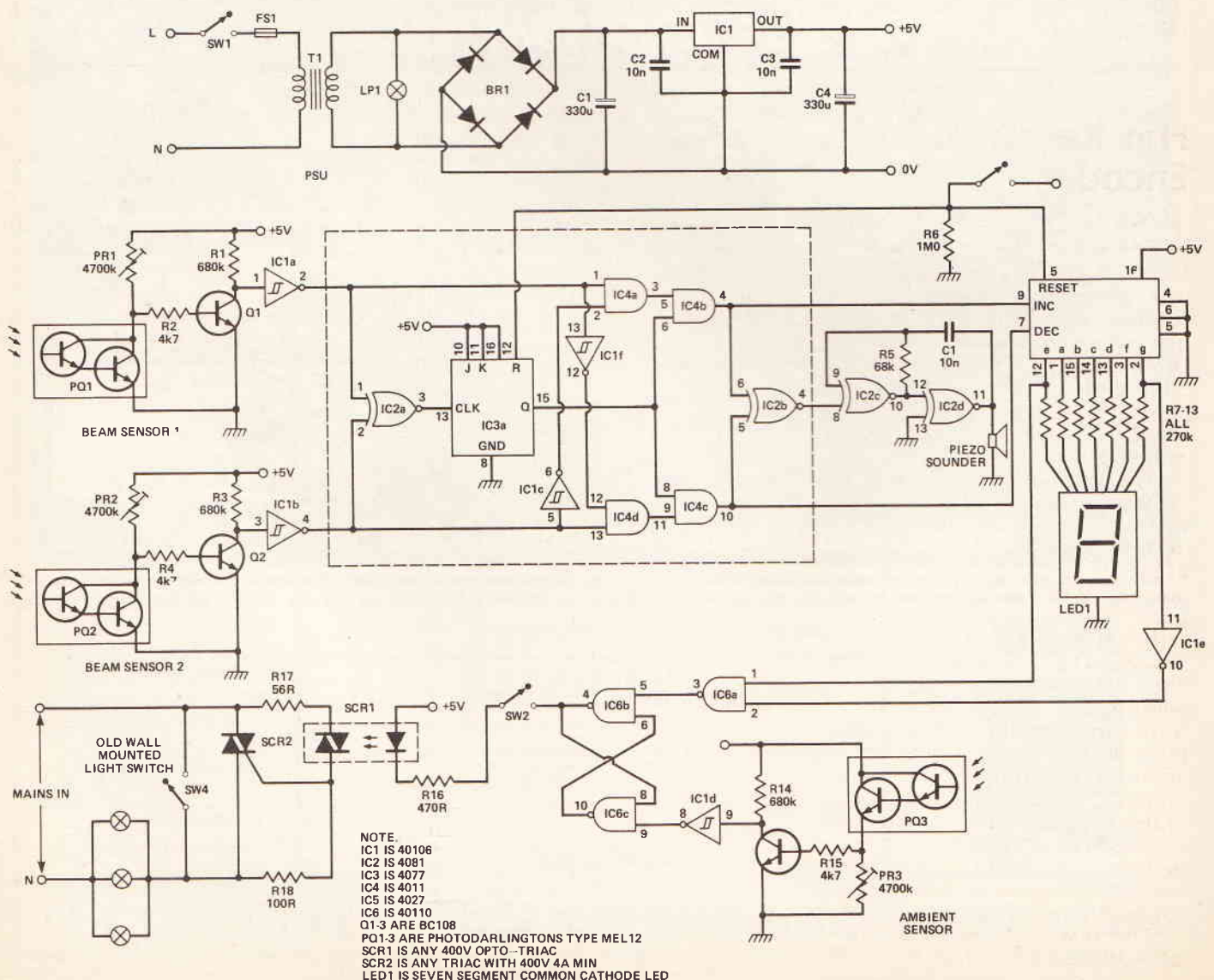
The figure opposite shows the timing of these signals; only in the final section, where the pulse from PQ2 has gone low again, do the conditions for the increment pulse to reach IC5 occur, which is when Q from IC3a and the output from IC1a are both high and the output from IC1b is low.

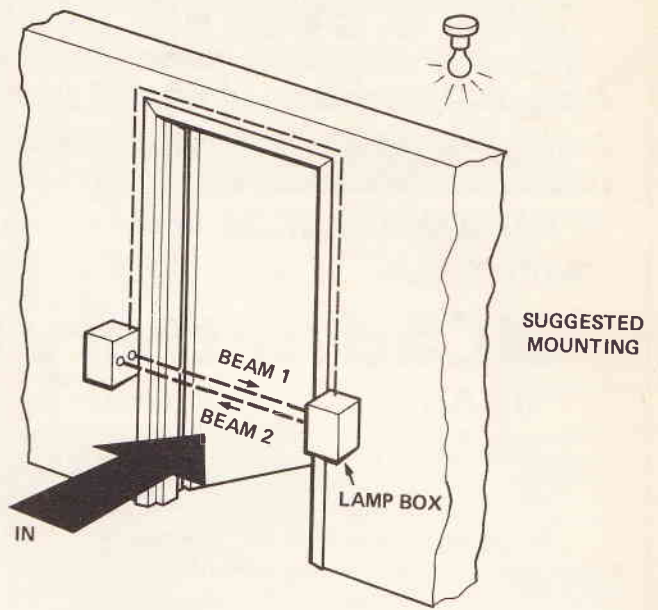
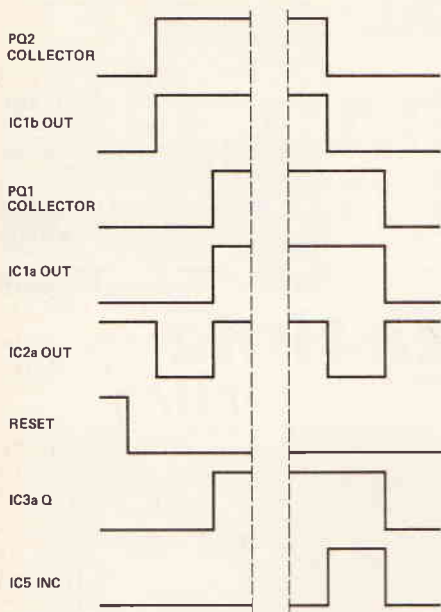
IC5 is an up/down counter seven-segment driver which counts the number of entries and exits from the room. IC1e and IC6a detect a

zero on the display. The latch formed around IC4b and c ensures that the light will only come on if there is no light falling on the ambient light detector, PQ3, but will then stay on until the room is vacated. The remaining circuitry for driving the triac via an opto-triac is quite straightforward.

SW2 is an auto/manual switch; SW3 is the reset switch, which should be used at switch-on and whenever the household children set about trying to confuse the unit.

A suggested method of construction is shown in the diagram. Standard three-core mains cable can be used to link the unit to the existing switch-plate (the cable carrying live, neutral and triac return) but note that the unit should be powered from a separate supply, and that it must be earthed to be safe. A metal box can be used to house all the phototransistors and the circuit





board and transformer; the beam sensors will need light-shielding tubes (sawn off felt tip pens could be used or something similar) which can be directed at a single light-source fitted on the opposite side of the door frame.

The ambient light sensor may need to be mounted separately, as the box may have to be mounted outside the room, depending on the direction that the door opens. The ambient light detector must be arranged so that it picks up light

from only the room being monitored.

An alternative to visible light beams would be to use modulated infra-red beams, but this involves extra complexity, which is why visible light was chosen.

Hex Keyboard Encoder

Adam Strange
Carrickfergus

While designing a micro system, I had to decide between using a software or a hardware hex keyboard encoder, and settled on the latter. Out came the good old Texas bible and the scratch pad. Some time later I came up with this little circuit which, even though I do say it myself, works rather well.

The heart of the circuit is IC1 ('LS93), a four-bit binary counter, which addresses IC2 and 3, which in turn scan the keyboard. IC3 ('LS156) is a two-to-four line decoder with open collector outputs. The two-bit address, A,B, selects which of the four outputs is low. IC2 ('LS173) is a four-to-one-line data selector; the two-bit address, A,B, selects which line is tested, the output Y going low when the selected input is low. So the address on the outputs of IC1 when output Y of IC2 is low is the address of the key pressed. (IC2 and 3 are dual devices, only one half of either being used here and alternative pin numbers are given where these are applicable on the circuit diagram).

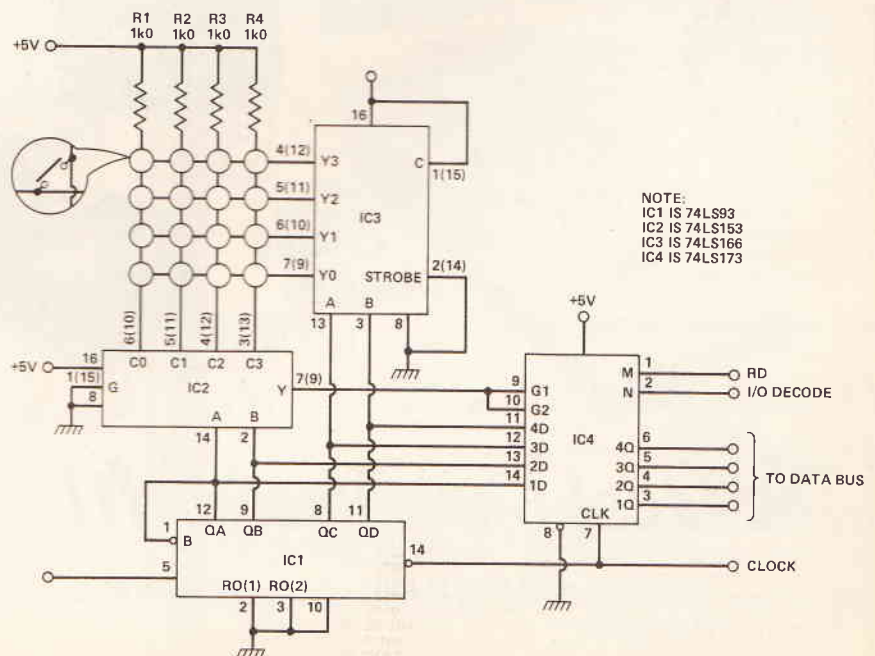
The next step was to capture or latch this address. This is accom-

plished by IC4 ('LS173) which is a four-bit D-type register with tri-state outputs (handy for CPU data bus). When the clock pulse goes from high to low the address from IC1 is incremented. This address is clocked into IC4 only if output Y and IC2 is low, this occurring on the low-to-high clock transition. Thus IC4 will hold the code of the last key to be pressed.

All that remains is for the CPU to

read the data from IC4. This occurs when the I/O decode and the RD inputs are low.

A cheap way to make the keyboard is to use an old calculator, replacing the original PCB with the one for the encoder. Suitably designed, the PCB for the encoder could be made to fit inside the calculator case — and if the display is still working, this too could be pressed into service.



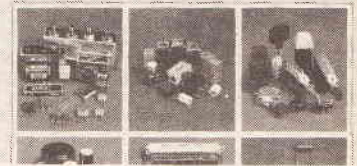
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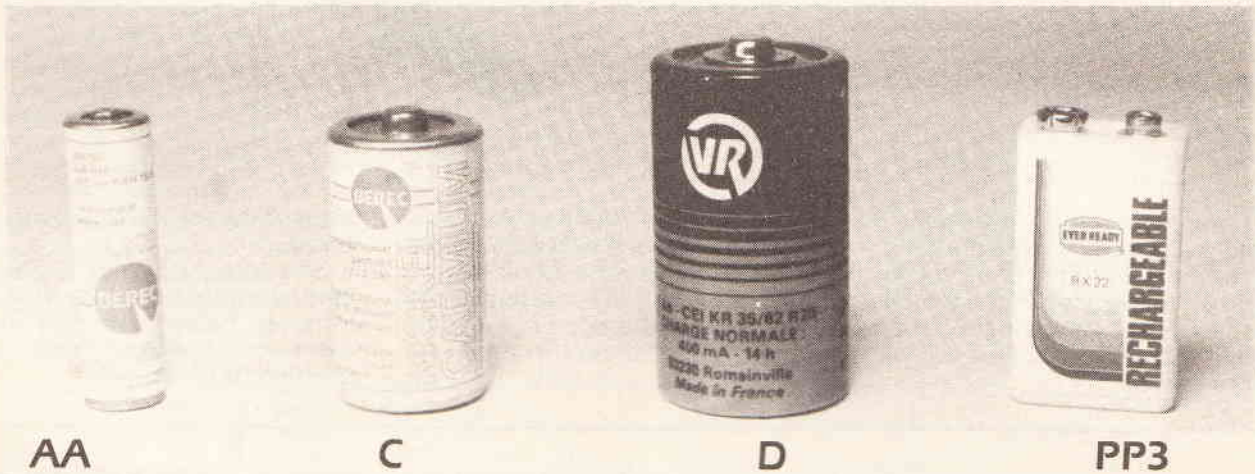
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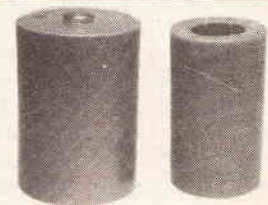
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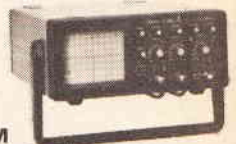
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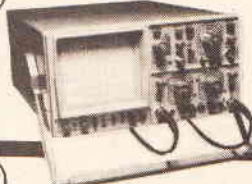
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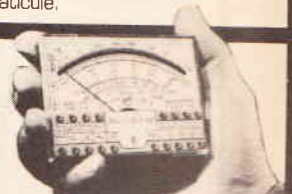
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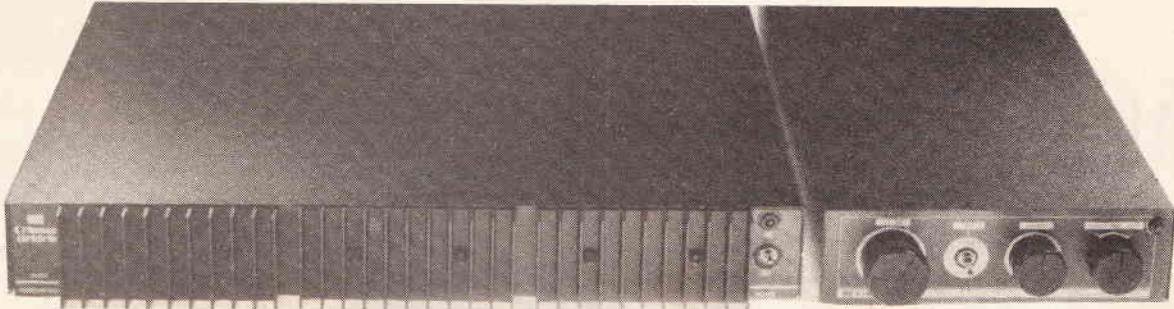


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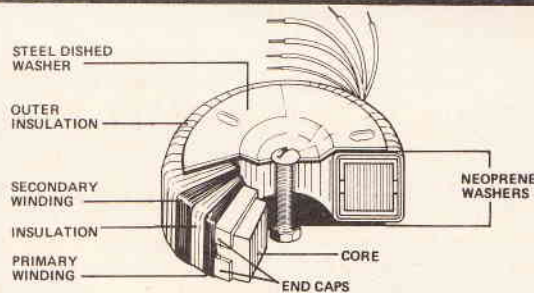
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MODULAR PREAMPLIFIER PART TWO

Some people are not happy unless they have a mass of controls not dissimilar to Concorde's flight deck on their side-board. The circuits here can help to extend the basic design, built using the modules featured last month, to include parametric tone controls, balanced output stage and a headphone amplifier.

A block diagram of the extended preamp is shown in Fig. 1, and apart from the increased circuitry, the main difference between this and the 'basic' design is that the volume control is no longer at the input. This obviously means that consideration has to be given to the possibility of overload. In Part 1, it was shown that the disc overload margin could be maintained at an adequate 32dB if the output level of the disc input stage was 200mV for its rated input. In order that this margin is not reduced, no gain may be introduced before the volume control, and the gain necessary to give a 1.0V output

should be made up by the output stage.

The input switching and tape buffer remain the same as in the simpler unit, but after the monitor switch, a unity gain buffer amplifier presents a high input impedance to the line inputs, and provides a low impedance drive to the tone control circuitry. The attenuator on the compact disc input is not to avoid overload, as the input and tone control circuits will easily handle the output of any CD player. Its purpose is to limit the signal level so that the volume control is not operated at a setting where its inter-track balance is not likely to be better than 3 or 4dB.

Tone Controls

Although fully paid-up members of the Flat Earth Society would have us believe that any form of signal processing is guaranteed to make a pig's ear of the emotional experience of listening to a group of musical morons twanging guitars and wailing in voices more suited to Billingsgate than Covent Garden, it should be remembered that most recordings are subject to considerable amounts of 'equalisation', usually to satisfy the producer's requirement for a particular type of sound. No allowance is made for the introduction of random phase shifts, or that the intricate

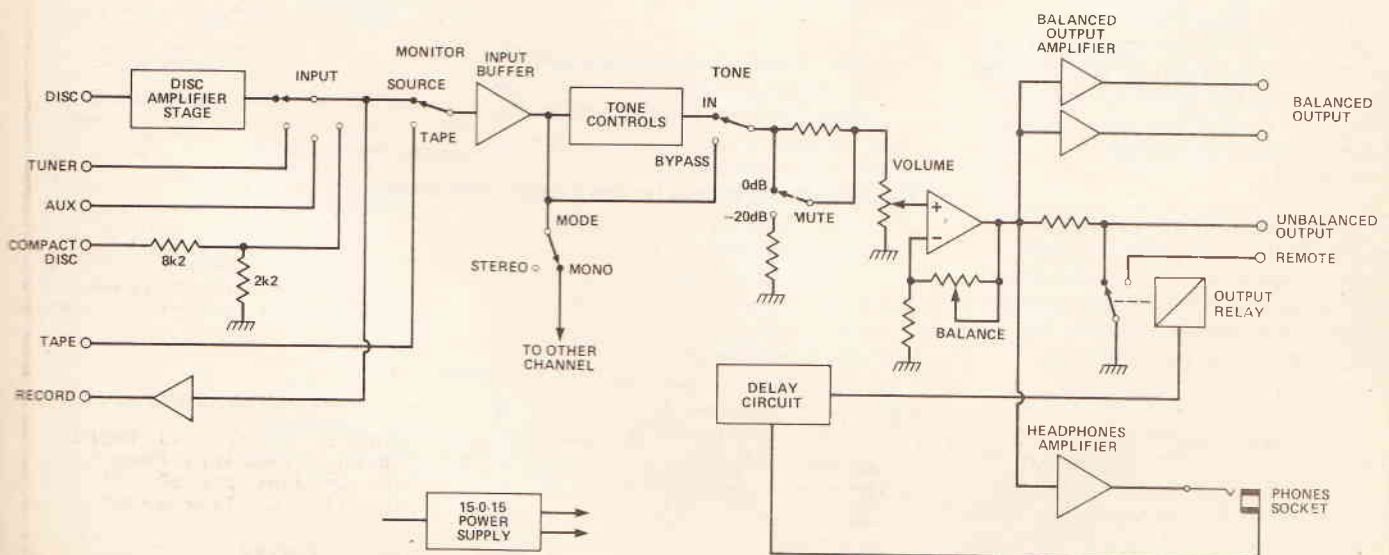


Fig. 1 Block diagram of the extended preamp.

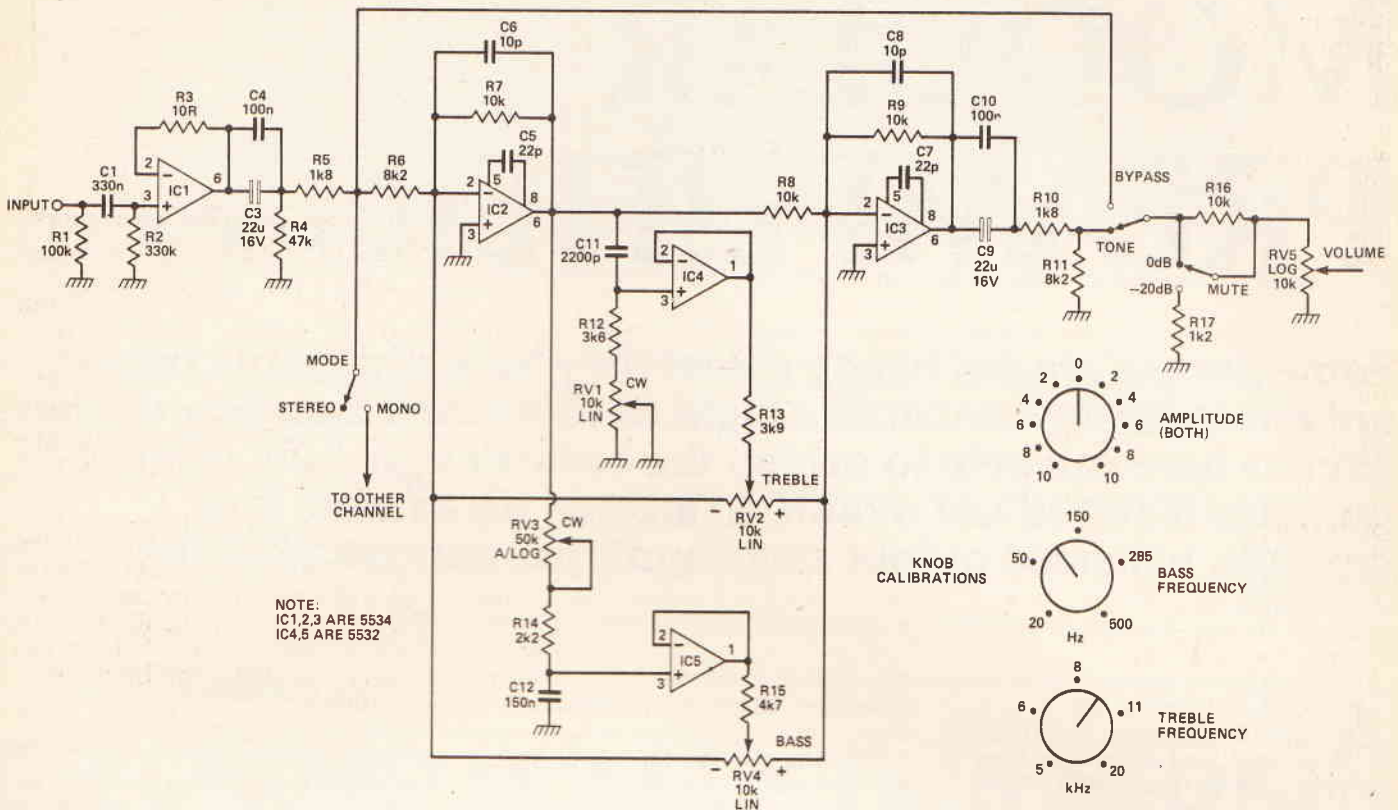


Fig. 2 Circuit diagram of the tone control module.

relationship of harmonics is sent on a one way trip to the cleaners. The object is to change the sound to make it more satisfactory, and if tone controls are used in the replay process for exactly the same purpose, surely no-one has the right to complain?

The type of tone control fitted to most hi-fi equipment is far from ideal, usually being much too dramatic in operation — for example, if it is required to lift frequencies below about 100 Hz, the effect is usually to lift, by varying amounts, everything up to at least 1 kHz, and even higher.

The circuit shown in Fig. 2 is somewhat more sophisticated than usual, possessing in addition to the normal lift and cut controls, adjustment of the turnover frequencies of the two sections.

Operation of the circuit is quite straightforward. IC1 acts as an input buffer, presenting an input impedance of approximately 100k ohms to the line inputs of the pre-amplifier. The input of IC1 is AC coupled by C1, which together with R2 fixes the -3dB point at

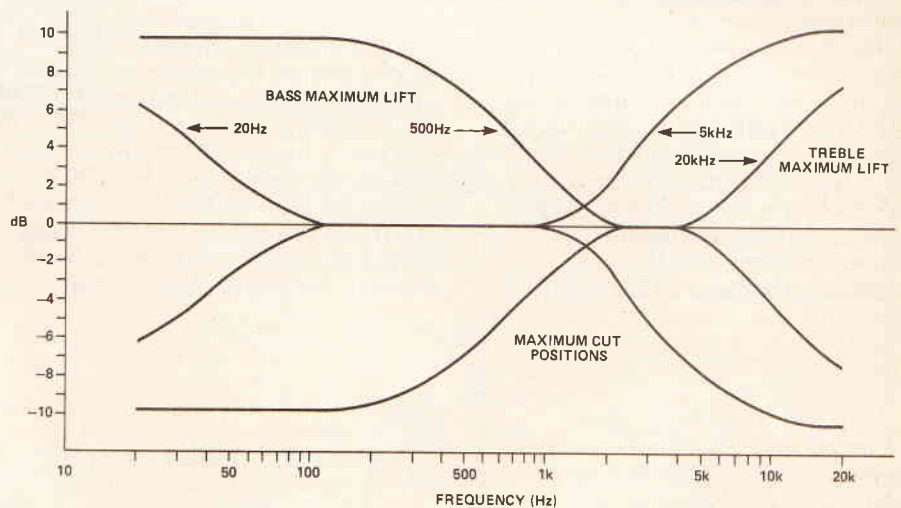


Fig. 3 Response curves for the tone control module.

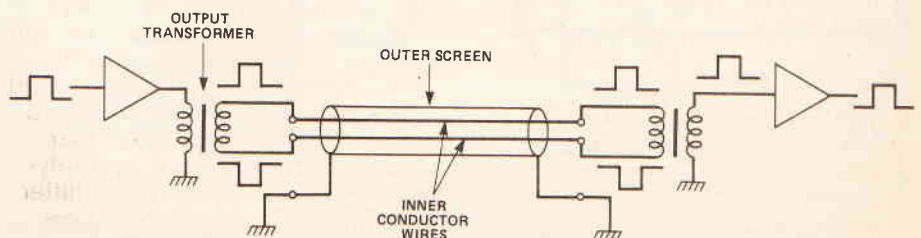


Fig. 4 The basic principle of balanced line operation.

PROJECT : Modular Preamplifier

about 1.5 Hz — low enough to prevent objectionable low frequency phase shift. The output of IC1 drives the pair of inverting stages formed by IC2 and IC3, the input resistor to IC2 being split to allow mono summing of the two channels. The signal path is maintained at unity gain by the equal input and feedback resistors of the two stages.

The output of IC2 feeds two single-pole filters which are buffered by IC4 and IC5. The filter formed by C11, R12 and RV1 has a high pass characteristic with its -3dB point adjustable by VR1 from 5.3 kHz to 20 kHz. Operation of the treble control, RV2, decides the destination of the high frequencies that emerge from the output of IC4 — in the "cut" position they are applied as negative feedback to IC2, and in the "lift" position they bypass R8 giving additional gain to IC3. The amount of lift and cut is controlled by R13, the value specified giving a ± 10 dB variation.

The bass control works in the same way, except that a low pass filter comprising C12, R14 and RV3 selects the low frequency range which is variable between 20 Hz and 480 Hz.

This type of tone control is characterised by shelving response curves with no interaction between the bass and treble sections. The curves are shown in Fig. 3 which illustrates the range of the variable frequency controls.

As the tone control section is non-inverting from input to output, it can readily be bypassed as shown. To ensure that there is no change in level when the bypass switch is operated, the 2.9dB attenuator formed by R5, R6 and the volume control is duplicated by the addition of R10 and R11 at the output of IC3.

The mute switch has been added, as much for convenience as anything. When changing records or when the 'phone rings it is very useful to be able to reduce the overall gain without disturbing the volume control setting.

Output Stage

The volume control is followed by the unbalanced output stage, already described in part 1. However, in order to give an additional 2.9dB of gain (to counteract the loss in the tone control circuit) the values of R4 and R6 should be changed to 133R and 300R respectively. The balance control characteristics are very slightly changed by this, as shown in Table 1, but they will still remain accurate to the calibrations.

In normal circumstances, the unbalanced output stage is all that will be needed. The main advantage of using a balanced output stage is realised when the signal output from the preamp has to run more than a metre or two, where the balanced output will give a much better noise immunity, or in an intrinsically noisy situation, eg disco systems, where the lighting controller can interfere with the audio signal.

As far as the user is concerned, the only difference between balanced and unbalanced lines is that balanced ones use a three-wire connection per channel instead of the usual two. Balancing has been standard with professional audio equipment since the days of 2LO and the cat's whisker (and Angela Rippon?), where it is used to ensure reliable, hum-free connections over long distances.

The basic principle is shown in Fig. 4; the signal is carried along two wires with the outer screen acting as an earth connection. The signal is inverted in one wire with respect to the other, but any hum and noise picked up from external signal sources by the cable will have the same phase in both wires. The balanced input accepts the differential signal, but rejects the externally introduced common mode signal. The normal method of balancing has traditionally relied upon the use of special input and output transformers, but similar results can be obtained by applying standard operational amplifier techniques — after all, the common op-amp has differential inputs.

Control Calibration	Channel Imbalance
2	1.87dB
4	3.78dB
6	5.79dB
8	7.96dB
10	10.39dB

Table 1 Balance control performance when used with tone control.

A balanced output consists of two outputs of identical levels but with one signal phase-inverted with respect to the other. Fig. 5 shows three ways that this could be achieved, and any one of these methods would be quite adequate provided it was connected to a balanced input. It may be seen that in each case, attenuation is introduced to ensure that half the input voltage appears at each output, but with opposite polarities. Thus a 1 volt input would result in outputs of +0.5 V and -0.5 V, giving the required 1 volt between conductors.

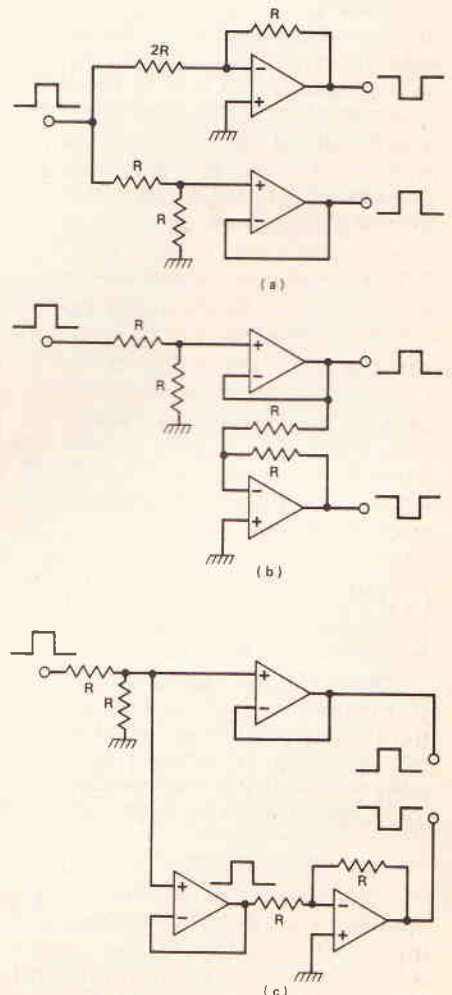


Fig. 5 Possible balanced output arrangements.

PROJECT : Modular Preamplifier

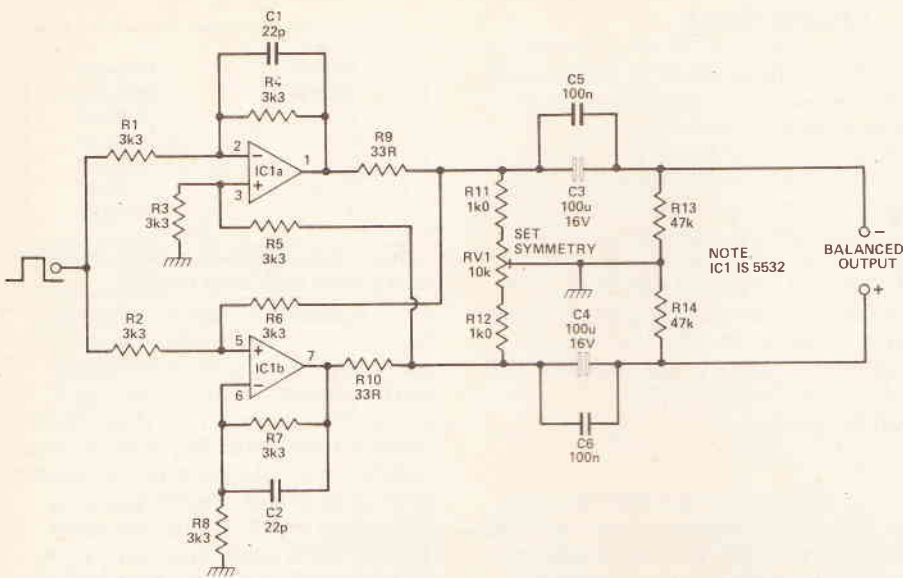


Fig. 6 Circuit diagram of the balanced output stage.

This is fine until the output is connected to an unbalanced input, when one of the balanced feeds gets shorted to earth, leaving a single output of 0.5 V. A difference of 6dB appears between balanced and unbalanced operation, which is not really acceptable. What is required is a method of increasing the gain of either output amplifier by 6dB whenever the other output is grounded, and such a circuit is illustrated in Fig. 6.

Here, the cross feed-back fixes the gain of each side at 0.5, but shorting either output to earth will remove this feedback, increasing the gain of the unshorted side to unity. As the balance condition of the circuit is extremely critical, the pre-set potentiometer is used to set the two outputs equal with respect to earth.

The whole object of the balanced output is that it should be connected to a balanced input. As these are not common in domestic equipment, a suitable circuit is given in Fig. 7, which is similar to the line input stages common in professional studio equipment (alternatively, see ETI may 1983 — Editor). This stage should be included in any equipment that is driven by the balanced output of the pre-amplifier while placed a considerable distance from it — active speakers and speaker-located amplifiers being the obvious cases in domestic systems.

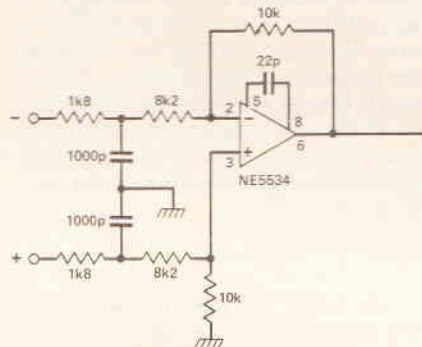


Fig. 7 A possible balanced input arrangement.

As shown in Fig. 1, the unbalanced output from the balanced line output stage is taken to the rear panel via the delay relay. This output will therefore be shorted to earth for about five seconds when power is first applied, and will also be cut off whenever a pair of headphones is plugged into the front panel-mounted jack socket.

Headphone Amplifier

Although most moving coil headphones have impedances in the 150 to 600 ohms range, the odd maverick pair are around that are as low as 8 ohms, so to be universal a headphone amplifier needs to be able to supply somewhat more current than a normal op-amp can manage. Various power ICs have been tried, but they all draw rather high quiescent current, causing the power supply regulators to get a bit too warm for comfort.

The circuit given in Fig. 8 uses an NE5534 to drive a pair of complementary transistors which are turned on by the voltage drop across R8. When the amplifier is in its quiescent state, the output stage is turned off, so minimum standing current is drawn. The transition point of the output devices does introduce some cross-over distortion, but this is kept within reasonable limits by negative feedback action, and the performance is more than adequate for headphone listening. The output resistor, R11, may be changed to suit the type of headphones in use, possibly requiring an increase to about 200 ohms with some medium impedance models.

Constructional details, overlay diagrams, etc for these modules will be given next month along with further information on the mother board. We will also be giving details of a series of kits of the hard-to-find parts, but in the meantime PLEASE don't ring us — just try to hold out a little longer, OK?

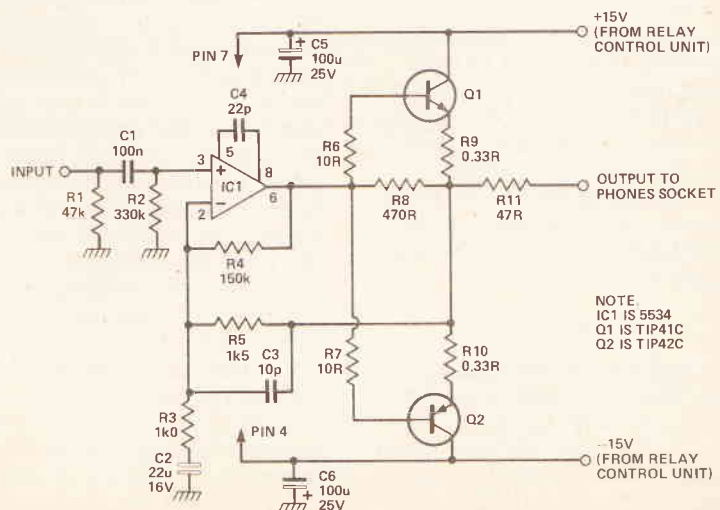


Fig. 8 Circuit diagram of the headphone amplifier module.

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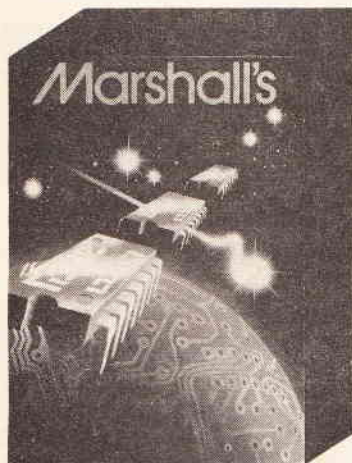
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UNIVERSAL EPROM PROGRAMMER

Revisited

We really started something with our Universal EPROM Programmer in the August and September issues. Requests for the assembler listing and for advice on how to modify the program to run on other machines continue to pour in. In an attempt to stem the tide, Mike Bedford offers a few further thoughts and the listing itself.

As mentioned in the 2nd part of the Universal EPROM Programmer article, the software has been written in such a way as to make it compatible with all 6502 based computers with the absolute minimum of changes. However, it is inevitable that some slight modifications will be required when transferring software, however similar the two machines may be. A large proportion of the software package is written in BASIC which, being a high level language, means that it should be possible to transfer it directly to another machine without any changes at all. This isn't quite the case as there are a number of dialects of BASIC, generally differing in those areas which are extensions to the original BASIC. Possible areas in which the BASIC program might need modifying have already been mentioned and it is now appropriate to indicate how the assembler subroutine may be modified to run on different machines.

Since all the keyboard and display I/O is carried out in the BASIC program hence camouflaging any hardware differences in these areas, the only changes which may be required to the assembler routine are due to differences in the memory maps and the clock speeds of the various machines. Apart from users wishing simply to transfer the software to another

machine, others may be interested in enhancing the package to carry out additional functions, for example, implementing the intelligent programming algorithm or adding new devices such as the 27256, 68732 and 68764 EPROMS which the hardware could support. It is therefore quite likely that a number of readers will require a much greater insight into the workings of the assembler routine than could be glimpsed from the hexadecimal dump given in the second part of the article. For this reason it is the intention here to reproduce a full assembler listing together with a simple "guided tour" to give some idea of how it works, hence enabling changes to be carried out without too much of the anguish often associated with trying to understand someone else's assembler program.

A few comments about the assembler are appropriate before going on to describe the structure of the program. Although all assemblers carry out essentially the same task there are often slight differences in the syntax. This program was written on a PDP-11 computer using a cross-assembler:

- The .PROCESSOR directive on line 13 is used to inform the assembler of which processor is in use. For 6502 only assemblers this line should be omitted.
- The .ORG directive on line 14 sets the start address of the code.

Syntax on other assemblers may be $\star=IC00H$ or $\cdot=IC00H$.

c). This assembler uses a suffix of H to indicate a hexadecimal number. Some other assemblers use a prefix of \$. Ie IC00H may need replacing by \$IC00.

d). In this assembler the .DEFINE directive is used to equate values to literals. In many other assemblers the word .DEFINE should be omitted to leave an equation (eg IC1PIA = OBC20H) and in others the EQU directive is used.

e). The .BYTE directive reserves a byte of memory and assigns an initial value to it. The more common version of this directive is DFB or DEFB.

The assembler syntax having been clarified, we can now go on to investigate the workings of the assembler subroutine and we shall make a start by looking at the parameter storage and data areas.

LOADR and HIADR are initialised by the BASIC program to one less than the first RAM address to be accessed. On exiting from the subroutine these locations will contain one more than the last address accessed. LOADE and HIADE are a similar address pair for the EPROM address. LOADF and HIADF are an address pair which are set by the BASIC program to one more than the last RAM address which should be used. RDATA is used to pass the

value of the data read from the EPROM back to the calling program, this being required in verify mode. MODE is set by the BASIC program to indicate whether read, verify, test or program function is required. Finally TYPE is set up by the main program to indicate the type of EPROM in use and will contain a number in the range 0 for 2758 to 8 for 27128.

As we now start to consider the data tables we shall be directing our attention to lines 47 to 64 of the program. In each of the seven lists here, there are 9 values of which one will be selected according to the value of TYPE. READS3 and READS6 contain the initial values of IC1CRB and IC2PIB respectively prior to which toggling bit 3 of IC2CRA would cause a read of the EPROM. PROGS5 and PROGS6 are similar tables of data for setting initial values of IC2CRA and IC2PIB prior to programming. PTBIT and PTBYTE indicate which bit of which PIA register requires to be toggled in order to carry out the programming of an EPROM. As a matter of interest, the reason that there are not tables of initial conditions for program and read for all PIA registers which connect to control pins on the EPROM is that some are set to the same initial value independently of EPROM type and some are set to the same value for both read and program. Finally A11A12 indicates whether the particular EPROM has A11 on pin 23 and A12 on pin 2 or A11 on pin 20 and A12 on pin 23, these being the two options for the 27-series and 25-series devices.

Having described the parameter storage and data areas it should be relatively straightforward to see how the assembler routine works. The value of MODE is used to select one of the two main routines either READ for reading, verifying or testing or PROG for programming. In either of these two

Table 1 The assembler listing. Note that:-

1). All pound signs (£) in this listing should be read as hash signs (#). It is purely a function of the printer used that these have been reproduced incorrectly.

2). The assembler listing refers to the two 6821 PIA's as IC1 and IC2 as was the case on the first prototype. IC1 should now be read as IC9 and IC2 as IC8. This in no way alters the operation of the software.

```

1      ;*****
2      ;*
3      ;* EPROM PROGRAMMER SUPPORT PACKAGE
4      ;* READ/PROGRAMME ROUTINE
5      ;* M. D. BEDFORD MARCH 1983
6      ;* THIS ROUTINE IS CALLED FROM A MAIN BASIC PROGRAM
7      ;* AND WILL SUPPORT 2758, 2716, 2516, 2732, 2732A
8      ;* 2532, 2764, 2564 AND 27128 DEVICES.
9      ;*
10     ;*****
11     ;
12     ;
13     ;       .PROCESSOR      R6500
14     ;       .ORG           1C00H
15     ;
16     ;ZERO PAGE LOCATIONS USED
17     ;
18     ;       .DEFINE       ZPLOAD=35H
19     ;       .DEFINE       ZPHIAD=36H
20     ;
21     ;ADDRESSES OF 6821 REGISTERS USED
22     ;
23     ;       .DEFINE       IC1PIA=0BC20H
24     ;       .DEFINE       IC1CRA=IC1PIA+1
25     ;       .DEFINE       IC1PIB=IC1PIA+2
26     ;       .DEFINE       IC1CRB=IC1PIA+3
27     ;       .DEFINE       IC2PIA=IC1PIA+4
28     ;       .DEFINE       IC2CRA=IC1PIA+5
29     ;       .DEFINE       IC2PIB=IC1PIA+6
30     ;       .DEFINE       IC2CRB=IC1PIA+7
31     ;
32     ;
33     IC00 4C4C1C      JMP      START
34     ;
35     ;
36     IC03 00      LOADR: .BYTE 0      ;LO RAM START ADDRESS
37     IC04 00      HIADR: .BYTE 0      ;HI RAM START ADDRESS
38     IC05 00      LOADE: .BYTE 0      ;LO EPROM START ADDRESS
39     IC06 00      HIADE: .BYTE 0      ;HI EPROM START ADDRESS
40     IC07 00      LOADF: .BYTE 0      ;LO EPROM FINISH ADDRESS
41     IC08 00      HIADF: .BYTE 0      ;HI EPROM FINISH ADDRESS
42     IC09 00      HIADM: .BYTE 0      ;HI ADDRESS EPROM MASKED
43     IC0A 00      RDATA: .BYTE 0      ;DATA READ FROM EPROM
44     IC0B 00      MODE: .BYTE 0      ;0-R, FFH-V, 80H-T, 2-P
45     IC0C 00      TYPE: .BYTE 0      ;0-2758 ... 8-27128
46     ;
47     ;INITIAL CONDITIONS FOR READ - IC1CRB, IC2PIB
48     ;
49     IC0D 3C      READS3: .BYTE 3CH, 3CH, 3CH, 3CH, 3CH, 3CH, 34H, 34H, 34H
50     IC16 18      READS6: .BYTE 18H, 18H, 18H, 10H, 10H, 18H, 12H, 10H, 12H
51     ;
52     ;INITIAL CONDITIONS FOR PROG - IC2CRA, IC2PIB
53     ;
54     IC1F 3C      PROGS5: .BYTE 3CH, 3CH, 3CH, 34H, 34H, 3CH, 3CH, 3CH, 3CH
55     IC28 08      PROGS6: .BYTE 8, 8, 8, 5, 25H, 8, 22H, 0, 22H
56     ;
57     ;BITS OF BYTES TO TOGGLE FOR PROGRAMME
58     ;
59     IC31 01      PTBIT: .BYTE 1, 1, 1, 1, 1, 8, 2, 8, 2
60     IC3A 06      PTBYTE: .BYTE 6, 6, 6, 6, 6, 5, 6, 5, 6
61     ;
62     ;PIN POSN OF A11/A12 1 * A11-PIN 23, A12-PIN 2
63     ; 0 * A11-PIN 20, A12-PIN 23
64     IC43 01      A11A12: .BYTE 1, 1, 1, 1, 1, 0, 1, 0, 1
65     ;
66     ;
67     IC4C 20B71D   START: JSR      ZPSWAP      ;SWAP RAM ADDR/ ZERO PGE
68     IC4F ADOB1C   LDA      MODE
69     IC52 C902     CMP      #2
70     IC54 D003     BNE     READ
71     IC56 4CB1C   JMP      PROG
72     ;
73     ;READING CODE
74     ;
75     IC59 A930     READ:  LDA      #30H      ;CONFIGURE
76     IC5B 8D25BC   STA      IC2CRA      ;IC2PIA
77     IC5E A900     LDA      #0
78     IC60 8D24BC   STA      IC2PIA      ;INPUT
79     IC63 A934     LDA      #34H
80     IC65 8D25BC   STA      IC2CRA      ;FOR
81     IC68 AEOC1C   LOOPR: LDX     TYPE      ;DEVICE TYPE INDEX
82     IC6B BD0D1C   LDA      READS3, X   ;SET
83     IC6E 8D23BC   STA      IC1CRB      ;UP
84     IC71 A900     LDA      #0
85     IC73 8D20BC   STA      IC1PIA      ;INITIAL
86     IC76 A93C     LDA      #3CH
87     IC78 8D25BC   STA      IC2CRA      ;CONDITIONS
88     IC7B BD161C   LDA      READS6, X   ;FOR
89     IC7E 8D26BC   STA      IC2PIB      ;READ
90     IC81 209C1D   JSR     DELAY
91     IC84 20621D   JSR     INCADD
92     IC87 D003     BNE     CONTR
93     IC89 4C131D   JMP     EXIT
94     IC8C 20171D   CONTR: JSR     SETAOD   ;SHORT DELAY
                                     ;NEXT RAM/EPROM ADDRESS
                                     ;IF NOT LAST - CONTINUE
                                     ;ELSE GO AWAY
                                     ;PUT ADDRESS ON PINS

```

PROJECT : EPROM Programmer

95	IC8F	AD25BC	LDA	IC2CRA	!SET
96	IC92	4908	EOR	£8	!CHIP ENABLE
97	IC94	8D25BC	STA	IC2CRA	!LOW
98	IC97	209C1D	JSR	DELAY	!SHORT DELAY
99	IC9A	AD24BC	LDA	IC2PIA	!GET DATA FROM EPROM
100	IC9D	8D0A1C	STA	HDATA	!AND STORE IT
101	ICA0	A200	LDX	£0	!ZERO INDEX REGISTER
102	ICA2	AC0B1C	LDY	MODE	!READ, TEST OR VERIFY ?
103	ICA5	F010	BEQ	RR	!READ
104	ICA7	3007	BMI	VV	!VERIFY
105	ICA9	C9FF	CMP	£OFFH	!MUST BE VERIFY - FF ?
106	ICAB	F0BB	BEQ	LOOPR	!IF SO ROUND AGAIN
107	ICAD	4C131D	JMP	EXIT	!ELSE NOT ERASED - EXIT
108	ICB0	C135	VV: CMP	(ZPLOAD,X)	!COMPARE WITH RAM
109	ICB2	F0B4	BEQ	LOOPR	!IF OK LOOP
110	ICB4	4C131D	JMP	EXIT	!ELSE BAD EPROM-EXIT
111	ICB7	8135	RR: STA	(ZPLOAD,X)	!STORE DATA IN RAM
112	ICB9	4C681C	JMP	LOOPR	!ROUND AGAIN
113					
114					!PROGRAMMING CODE
115					
116	ICBC	A930	PROG: LDA	£30H	!CONFIGURE
117	ICBE	8D25BC	STA	IC2CRA	!IC2PIA
118	ICC1	A9FF	LDA	£OFFH	!AS
119	ICC3	8D24BC	STA	IC2PIA	!OUTPUT
120	ICC6	A934	LDA	£34H	!FOR
121	ICC8	8D25BC	STA	IC2CRA	!PROGRAMME
122	ICCP	AEOC1C	LOOPP: LDX	TYPE	!EPROM TYPE
123	ICCE	BD0D1C	LDA	READS3,X	!SET
124	ICD1	8D23BC	STA	IC1CRB	!UP
125	ICD4	A900	LDA	£0	!INITIAL
126	ICD6	8D20BC	STA	IC1PIA	!CONDITIONS
127	ICD9	BD1F1C	LDA	PROGS5,X	!FOR
128	ICDC	8D25BC	STA	IC2CRA	!PROGRAMME
129	ICDF	BD281C	LDA	PROGS6,X	!
130	ICE2	8D26BC	STA	IC2PIB	!
131	ICE5	209C1D	JSR	DELAY	!SHORT DELAY
132	ICE8	20621D	JSR	INCADD	!NEXT RAM/EPROM ADDRESS
133	ICEB	F026	BEQ	EXIT	!IF LAST THEN EXIT
134	ICED	20171D	JSR	SETADD	!PUT ADDRESS ON PINS
135	ICF0	A200	LDX	£0	!ZERO INDEX REGISTER
136	ICF2	A135	LDA	(ZPLOAD,X)	!GET DATA FROM RAM
137	ICF4	8D24BC	STA	IC2PIA	!PUT DATA ON PINS
138	ICF7	AEOC1C	LDX	TYPE	!EPROM TYPE
139	ICFA	BC3A1C	LDY	PTBYTE,X	!BYTE TO TOGGLE
140	ICFD	B920BC	LDA	IC1PIA,Y	!LOAD IT
141	ID00	5D311C	EOR	PTBIT,X	!TOGGLE BIT
142	ID03	9920BC	STA	IC1PIA,Y	!PUT IT BACK AGAIN
143	ID06	A01D	LDY	£10H	!CARRY
144	ID08	A2FF	LDX	£OFFH	!OUT
145	ID0A	CA	DEL: DEX		!50 MS
146	ID0B	D0FD	BNE	DEL	!DELAY
147	ID0D	88	DEY		!FOR
148	ID0E	D0FA	BNE	DEL	!PROGRAMME
149	ID10	4CCB1C	JMP	LOOPP	!ROUND AGAIN
150					
151	ID13	20871D	EXIT: JSR	ZPSWAP	!SWAP BACK ZERO PAGE
152	ID16	60	RTS		!EXIT BACK TO BASIC
153					
154					
155					!ROUTINE TO PUT ADDRESS ON APPROPRIATE EPROM PINS
156					
157	ID17	AD051C	SETADD: LDA	LOADE	!WRITE LOW ORDER BYTE
158	ID1A	8D22BC	STA	IC1PIB	!STRAIGHT TO EPROM
159	ID1D	BD431C	LDA	A11A12,X	!25 OR 27 SERIES ?
160	ID20	F009	BEQ	ADD25	!BRANCH IF 25-SERIES
161	ID22	AD061C	LDA	HIAD5	!GET HI ORDER BYTE
162	ID25	8D20BC	STA	IC1PIA	!WRITE STRAIGHT TO EPROM
163	ID28	4C521D	JMP	ADD13	!JUMP TO A13 CODE
164	ID2F	AD20BC	ADD25: LDA	IC1PIA	!GET IC1PIA
165	ID2E	0D091C	ORA	HIADM	!OR IN MASKED HI BYTE
166	ID31	8D20BC	STA	IC1PIA	!PUT IT BACK AGAIN
167	ID34	AD061C	LDA	HIAD5	!GET HI ORDER BYTE
168	ID37	2910	AND	£10H	!TEST A12
169	ID39	F008	BEQ	ADD11	!IF UNSET GO TO A11 CODE
170	ID38	AD20BC	LDA	IC1PIA	!A12 IS SET - GET IC1PIA
171	ID3E	0908	ORA	£8H	!OR IN A12
172	ID40	8D20BC	STA	IC1PIA	!AND PUT IT BACK AGAIN
173	ID43	AD061C	ADD11: LDA	HIAD5	!GET HI ORDER BYTE
174	ID46	2908	AND	£8H	!TEST A11
175	ID48	F008	BEQ	ADD13	!IF UNSET GO TO A13 CODE
176	ID4A	AD26BC	LDA	IC2PIB	!A11 IS SET - GET IC2PIB
177	ID4E	0901	ORA	£1H	!OR IN A11
178	ID4F	8D26BC	STA	IC2PIB	!PUT IT BACK AGAIN
179	ID52	AD061C	ADD13: LDA	HIAD5	!GET HI ORDER BYTE
180	ID55	2920	AND	£20H	!TEST A13
181	ID57	F008	BEQ	ADDEXT	!IF NOT SET RETURN
182	ID59	AD23BC	LDA	IC1CRB	!A13 IS SET - GET AC2PIB
183	ID5C	0908	ORA	£8H	!OR IN A13
184	ID5E	8D23BC	STA	IC1CRB	!PUT IT BACK AGAIN
185	ID61	60	ADDEXT: RTS		!RETURN
186					
187					
188					!INCREMENT ADDRESS FOR BOTH RAM AND EPROM, WRITE

routines the initial conditions are set up and a loop is executed for each address to be read or programmed. Each time round the loop the appropriate PIA bit is toggled to carry out the required function to the EPROM. In the case of testing the read data is compared with FF (the expected value for an erased EPROM) and in verifying the read data is compared with data in RAM. In either of these two modes, if the test fails the subroutine exits and this is detected in the BASIC program by the fact that the address returned in LOADR and HIADR is less than the expected final RAM address.

The general overview being complete, a few specific points on the tailoring of the assembler routine to suit other machines will now be covered.

a). The origin of the routine should be selected so as not to conflict with the area of RAM used by the BASIC program and the area to be used for data storage (as selected by the BASE command). The origin is set on line 14.

b). The address of the EPROM programmer hardware as selected by the on board links should be equated to IC1PIA on line 23. It should be noted that the addresses in a). and b). must agree with the addresses of the M/C code routine and hardware as assigned in the BASIC program.

c). Lines 143 to 148 are a couple of nested loops which implement the 50ms pulse required for programming EPROMs. These loops will only generate a 50ms delay when running on a processor with a 750 kHz clock such as the Tangerine Microtan. For different clock frequencies the value of 1D loaded into register Y on line 143 would require to be changed proportionally. For example, if the subroutine were to be run on a machine with a 1MHz clock a value of 1D (hex) ★ 1000/750 = 27 (hex) should be used.

As a final point, although the assembler routine has been written for a 6502 processor and as such will not run on any other processor, the hardware is compatible with the increasing number of computers using the 6809 processor. For this reason, some owners of 6809 based machines may like to try their hand at converting this routine to 6809 code. Although, it wouldn't result in the most efficient 6809 code, the easiest way to do this would be to translate it virtually on an instruc-

PROJECT: EPROM Programmer

tion by instruction basis, a task which shouldn't be beyond the capabilities of those with a moderate knowledge of 6809 programming.

The following list contains all those errors which have come to light since the project was published.

On the circuit diagram (page 46, August 1983), C6 is 100µ and C9 is 100n, not the other way round as given. Some bars were omitted from note three of Table 1 on page 48: it should have read "CE/PGM (27 series) is equivalent to PD/PGM (not PD/PGM) (25 series)." The penultimate sentence of the first paragraph on page 50 should read "... adjust RV1 for a potential of +25 V at IC10 output." On the overlay, IC7 is between SK2 and SK1, IC6 is between SK1 and C10, IC11 is between R7 and R10, R3 is between R2 and Q2, and Q7 is between Q6 and Q8. A link is missing between IC7 and SK1, and the unidentified pins at the right hand end of SK3 are the +5V line. Finally, C10 appears twice in the parts list but only the first entry is correct, and the second DIL socket should of course, be 8, not 80, way.

Table 1 continued (see notes overleaf).

189				‡HIADM -IE HIADIE WITH A11 AND A12 MASKED OUT
190				‡AND SET Z CONDITION CODE IF LAST ADDRESS DONE
191				‡
192	ID62	E635	INCADD: INC	ZPLOAD ‡LO ORDER RAM ADDRESS
193	ID64	D002	BNE	INCROM ‡SKIP IF NO CARRY
194	ID66	E636	INC	ZPHIAD ‡ELSE INC HI RAM ADD
195	ID68	EE051C	INCROM: INC	LOADE ‡LO ORDER EPROM ADDRESS
196	ID6B	D003	BNE	INCEXT ‡SKIP IF NO CARRY
197	ID6D	EE061C	INC	HIADIE ‡ELSE IN HI EPROM ADD
198	ID70	AD061C	INCEXT: LDA	HIADIE ‡GET HI ORDER EPROM
199	ID73	29E7	AND	EOE7H ‡MASK OUT A11, A12
200	ID75	8D091C	STA	HIADM ‡STORE IT
201	ID78	AD051C	LDA	LOADE ‡GET LO EPROM ADDRESS
202	ID7B	CD071C	CMP	LOADF ‡LAST ADDRESS ?
203	ID7E	D006	BNE	INCRIS ‡IF NOT EXIT
204	ID80	AD061C	LDA	HIADIE ‡ELSE TEST HI ORDER
205	ID83	CD081C	CMP	HIADF ‡LAST ADDRESS ?
206	ID86	60	INCRIS: RTS	‡RETURN
207			‡	
208			‡	
209			‡THIS ROUTINE SWAPS ZPLOAD WITH LOADR	
210			‡AND ZPHIAD WITH HIADR	
211			‡	
212	ID87	A635	ZPSWAP: LDY	ZPLOAD ‡GET LO ZERO PAGE
213	ID89	A436	LDY	ZPHIAD ‡AND HI ZERO PAGE
214	ID8B	AD031C	LDA	LOADR ‡GET LO RAM
215	ID8E	8535	STA	ZPLOAD ‡WRITE TO LO ZERO PAGE
216	ID90	AD041C	LDA	HIADR ‡GET HI RAM
217	ID93	8536	STA	ZPHIAD ‡WRITE TO HI ZERO PAGE
218	ID95	8E031C	STX	LOADR ‡ZERO PAGE TO LO RAM
219	ID98	8C041C	STY	HIADR ‡ZERO PAGE TO HI RAM
220	ID9B	60	RTS	‡RETURN
221			‡	
222			‡	
223			‡SHORT DELAY TO ACCOUNT FOR CAPACITOR SLOWING	
224			‡SIGNALS ON PIN 22 (20)	
225			‡	
226	ID9C	A080	DELAY: LDY	EO80H ‡LOOP COUNTER
227	ID9E	88	DELAY: DEY	‡DECREMENT
228	ID9F	D0FD	BNE	DELAYI ‡LOOP IF NOT ZERO
229	IDA1	60	RTS	‡RETURN
230			‡	
231			‡	
			.END	

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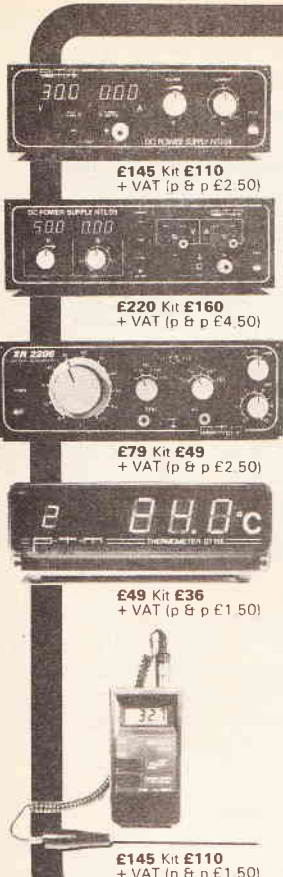
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2114 450ns Low power	.95	.85	.80						
6116/2016	3.35	3.00	2.85						
6116 150ns Low power	4.90	4.40	4.20						
2716 450ns 5 volt	2.69	2.40	2.30						
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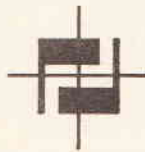
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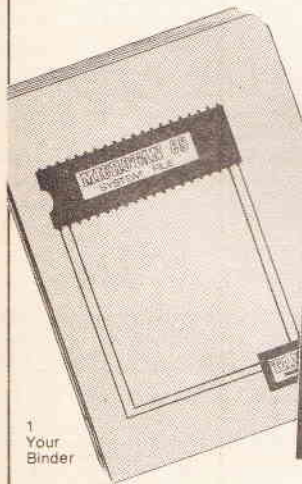
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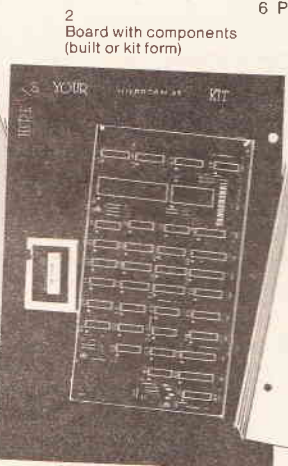
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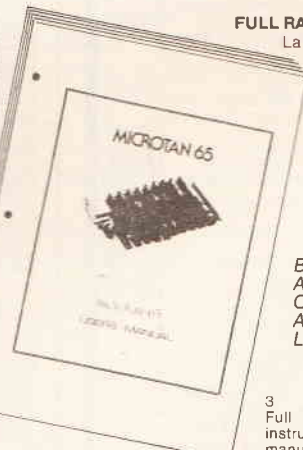
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BOOK REVIEWS

So you thought we couldn't read? Just to prove you wrong, the ETI staff has been ploughing through some of the new works in the field — here's what we think of them.

Understanding Digital Logic Circuits

**R.G. Middleton
Prentice/Hall International
392 pages/£16.10**

According to the preface, this book is aimed at those who are currently working in some area of electronics but who are not familiar with digital techniques. It assumes little or no prior knowledge either of the technology or the maths behind it and covers everything from the simplest of gates through to counters, converters, memories and the more complex devices now in use.

One of the first things one notices on reading through the book is that it is American, and that the illustrative examples used are therefore American also. Instead of the 74 series TTL and 4000 series CMOS familiar to British engineers, the notes and pin-out diagrams refer, with a few exceptions, to the Fairchild 93, 96, and 9N ranges, none of which are very well known in this country. Whilst this may not be a serious shortcoming it must, I feel, reduce the book's value and appeal to those at whom it is ostensibly aimed, that is, beginners in the field of digital electronics.

Another slight annoyance I found was the poor positioning of related text and illustration. This varied throughout the book, but in the worst instances as much as seven pages separated a section of text from the illustration to which it referred. In those places where a passage in the text referred to more than one illustration at a time, I very soon ran out of fingers! Whilst this, too, is perhaps a minor point it does make certain sections far more daunting than they need be, and again might well prove discouraging to those unfamiliar with the material.

On a more positive note, the book covers its ground very

thoroughly indeed and has a suitably authoritative feel to it. There would be few, I suspect, who could read through it without learning something of value. I am not at all convinced that it is the best introduction for those new to digital electronics, but it is an excellent reference book for those, like me, who learnt only analogue techniques during their periods of formal study and who have picked up digital theory piecemeal along the way. The index, if not exhaustive, is certainly adequate, and after a week or two I found myself turning to it automatically whenever something on the bench posed a question of a digital nature.

IJP

Microprocessor Technology

**David. L. Terrell
Prentice/Hall International
562 pages/£20.65**

This is a fairly readable delve into the inner mysteries of the Z80 microprocessor chip and some of its more common support devices. This book covers both the hardware and software aspects of actually using a microprocessor chip, providing numerous examples of each and it even contains a circuit diagram for a basic trainer unit.

On the software side, the book covers not only the Z80 instruction set in reasonable details but proceeds to show how to accomplish some of the more common tasks required of simple computer and control systems. This is backed up on the hardware side by basic interface circuitry and illustrations of how to drive them.

The Z80 processor which is the basis of the book is one of the more complex 8-bit devices generally available. This means

that while most of the concepts covered in the book are applicable to other devices, it must be remembered that different approaches may be required when realising systems using them.

Some knowledge of electronics and logic would be an advantage when reading the book as would access to some sort of small computer system and possibly someone with whom to discuss points of interest.

PJW

The Micro Cookbook

**Vol. 1
Don Lancaster
Prentice/Hall International
384 pages/£13.55**

Don Lancaster's Cookbook series has developed a good reputation for handling complex technical information in a down-to-earth practical way. In my experience, the most widely known is the CMOS cookbook, and this has graced many a lab bookshelf that I've known. So, the Micro Cookbook has a lot to live up to — but I'm afraid that it's blown it.

The first disappointment is that, as you may have already noticed, this is just volume 1 — volume 2, dealing with programming (machine code, of course), I/O, advanced techniques (no, they didn't say what that meant), and some detailed examples, is still on the rollers. The first volume is just the introduction!

Even so, it hasn't made up its mind who it's for. The others of the Cookbooks have all assumed that the reader has a firm grasp of the fundamentals but not necessarily the details. This Cookbook seems to be aimed at the *idiot savant* played by Richard Prior in 'Superman III' — one moment it's insulting your intelligence with some of the most crass technical writing I've come across (for example, one of the exercises given to readers is

"Show the Exclusive-Or logic involved in having two girlfriends"), the next it's assuming you know far more about microprocessors than it has bothered to explain to you.

This is not to say that the Cookbook has nothing to offer, there is a great deal that's useful, even entertaining in it, and it can be very difficult to put down. However, all this good is buried and difficult to find.

So, I'm afraid, a disappointment, which is a real pity, because I'm sure that done properly, this book could have been at least as useful as others in the series. Let's hope that volume 2 is an improvement.

DJB

The Ground Launched Cruise Missile: A Technical Assessment

Tim Williams

Electronics For Peace

36 pages/75p (£1 inc postage)

Before getting too far into this review,

a couple of confessions are in order. First of all, electronics for peace is 'a network... to link those working in electronics and computing who share a concern for the military implications of their profession.' Thus it is not a group that one would expect to be that well disposed towards cruise missiles in the first place, secondly, your reviewer is not that well disposed towards cruise missiles, either.

Confessions over, this book is reviewed here because it presents hard information in a subject area normally notable for the domination of opinion. Not that the author has been lent a GLCM to put through its paces; most of the technical details of the missile system are well-guarded secrets. However, using a very wide range of sources, the author has been able to build up a disquieting picture of the goings on in the GLCM programme.

For instance, it is possible to infer that the reliability of GLCMs is lower than that of other American strategic nuclear weapons because there is no independent contractor whose only responsibility is to ensure reliability — contrary to practice in

all other strategic weapon programmes.

The booklet catalogues likely technical problems, amongst which is that GLCMs use a very large number of advanced VLSI devices. Very few such devices have yet been approved to military specifications; also, there seems to be a problem in adequately sealing the chip encapsulation.

Another major problem area dealt with is the software. The software contractor is known to have run into difficulties — however, this is far from surprising, as a recent survey of US government software contracts found that only 1.7% of software could be used as delivered.

Whether you are for or against nuclear weapons in general or the stationing of GLCMs in this country in particular, or even if you simply have not made up your mind, this booklet raises questions that demand an answer. It is available from Electronics for Peace, 151 Courthouse Road, Maidenhead, Berks SL6 6HY.

DJB

Reviewers: PJW — Phil Walker; IJP — Ian Pitt; DJB — Dave Bradshaw.

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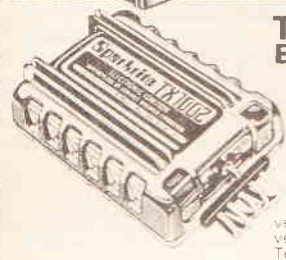
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AT-40 Electronic Car Alarm

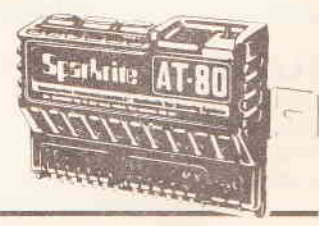
- Guards doors, boot, bonnet from unauthorised entry ● Armed/disarmed using concealed switch ● 30 second delay-to-arm ● 7 second entry delay ● Can alternatively be wired to exterior key switch ● Flashes headlights & sounds horn intermittently for 60 seconds when activated ● Security loop protects accessories ● Low consumption C-MOS circuitry.



NEW

AT-80 Electronic Car Security System

- Guards doors, boot, bonnet from unauthorised entry ● Armed/disarmed from outside vehicle by magnetic key fob passed across sensor pad adhered to inside of windscreen ● Individually programmable code ● 30 second delay-to-arm ● Flashes headlights and sounds horn intermittently for 60 seconds when activated ● Security loop protects accessories ● Function lights to assist setting-up ● Low consumption C-MOS circuitry.



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- Supplementary to AT-40 & AT-80 ● Will work in conjunction with any door switch input or voltage sensing alarm ● Detects attempted break-in and movement within passenger compartment & triggers alarm ● Includes high efficiency ultrasonic transducers ● Crystal controlled for low drift ● Ingenious sensitivity control allows freedom from false alarms ● Low current consumption



NEW

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IC UPDATE

This month, an IC for the enthusiast who has everything, including a generous overdraft facility: digital to analogue converter for colour video. Certainly, it's state-of-art; equally certainly, it's expensive.

This hybrid digital to analog converter provides three channels of video output for RGB type video displays with picture element (pixel) rates to 40MHz. The RGB DAC contains three video DACs and three RAM arrays (16 x 4) as well as all control inputs required to generate output waveforms which are compatible with EIA standards RS-170 and RS-343 (see Fig. 1).

The RGB DAC 4T provides four bits of resolution or 16 levels of "gray scale" per color. This gives the user a $(2^4)^3$ or 4096 color palette. The 16 x 4 ram array per colour allows the user a choice of any 16 of the 4096 colours for each sweep. The write speed is also high enough to allow the colour map to be updated during the vertical retrace or even horizontal retrace in some systems. The high update rates and the ability to generate a full 1 volt composite video output across a 75 ohm load makes this DAC ideally suited for colour computer graphics using raster scan technology.

FEATURES

- 4096-colour palette
- Three video DACs
- Update rates to 40 MHz
- Complete composite video capability
- 16 by 4 bit colour map RAM
- TTL compatible
- Direct 75 ohm RGB outputs
- Clean glitch-free output
- Single +5V supply

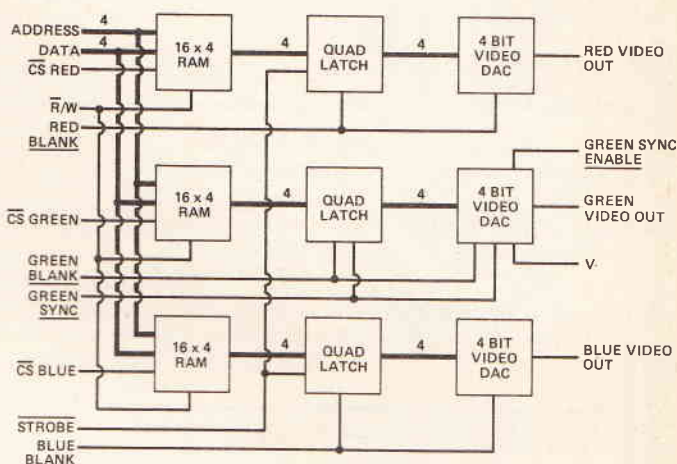


Fig. 1 Block diagram. Fig. 2 RGB DAC 4TD connections.

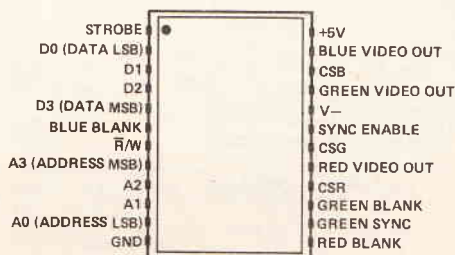


Fig. 2 RGB DAC 4TD connections.

PIN DESCRIPTIONS

STROBE

The transition from Logic 1 to Logic 0 transfers data from RAM outputs to the data register outputs. The strobe is not used for write operations.

GREEN SYNC (composite sync)

A logic 1 sets the registers to all 0s (ref black) and drives the green output to a level 286mV more negative than the reference black level. This signal has priority over blanking and data inputs from the RAMs and is used to synchronize the beam traces in a raster scan type display.

BLANKING (Red, Grn, Blu)

A logic 1 sets the registers to all 0s (ref black) and drives the output to a level 50mV more negative than the reference black level. This signal has priority over the data inputs from the RAMs and is used to shut off the beam for the darkest display possible.

SYNC ENABLE

This input should be connected to +5V to enable the sync signal feature of the green output. If this feature is not desired this input should be connected to ground.

-V

This input should be connected to a stable -3 to -15 volt supply to restore the green output blanking level to 0V absolute if the sync enable is connected to +5V. If it is not necessary to restore the green output blanking level to 0V or if sync enable is grounded this pin should be grounded.

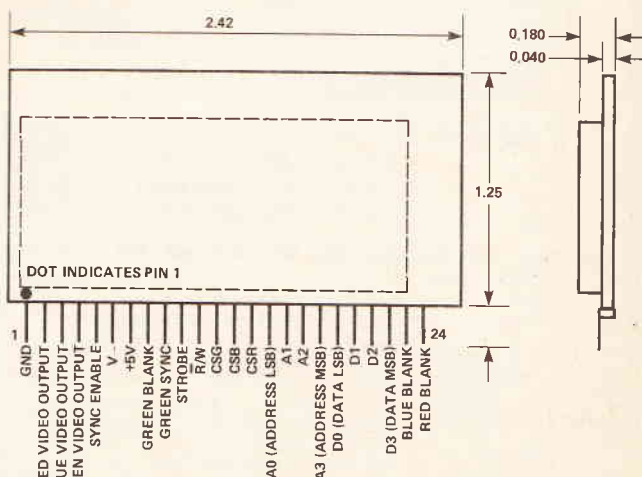


Fig. 3 RGB DAC 4T connections.

ADDRESS — 4 Bits — A0, A1, A2, A3.

Determines read or write address for all RAM arrays. These inputs are used as an address input to load arrays in the write mode and as data inputs during the read (display) mode.

DATA — 4 Bits — D0, D1, D2, D3

Used to load data to all RAM arrays — data loaded will be non-inverted to the DAC during read mode.

R/W

Logic 0 selects read operation
Logic 1 selects write operation

All data to DAC registers will be logic 1 during write mode. If no strobe signal is applied during write operations, the DAC outputs will retain the last read operation level. Otherwise the outputs will rise to REF WHITE level unless composite sync (green output) or blanking signal is applied.

CSR, CSG, CSB

Chip select for each channel (red, green, or blue) A logic 0 selects RAM channel for read or write operations and a 1 deselects RAM for any operation. If deselected, the data to the DAC registers will be logic 1. If no strobe signal is applied while the RAM is deselected, DAC outputs will retain the last read operation level. Otherwise the output will rise to REF WHITE level unless composite sync (green output) or blanking signal is applied. Normally only one input is enabled (logic 0) to write data to its corresponding RAM and all inputs are enabled (logic 0) to read data during display.

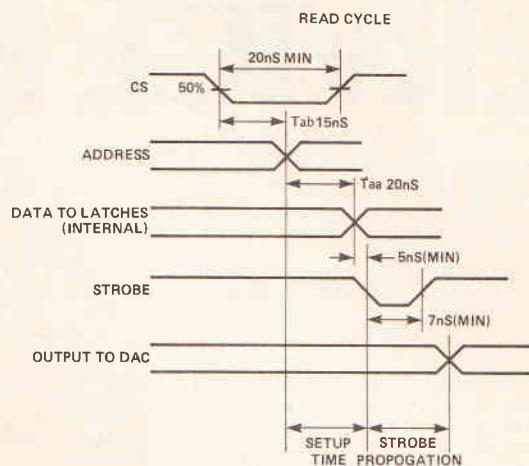


Fig. 4 Read cycle timing diagram.

SPECIFICATIONS

(Typical @ +25°C, +5V and 75 load unless otherwise stated).

RESOLUTION	PARAMETER	UNITS
4		bits
PALETTE	4096	colours
	(16 colours per sweep)	
ANALOG OUTPUTS (each channel)		
Voltage range (1%)	0 to 0.6	volts
Current (75 ohm load)	-17	mA
Impedence ($\pm 5\%$)	75	ohms
Compliance	± 2	volts
OUTPUT — COMPOSITE SYNC		
Green Only	-286	mV ($\pm 5\%$)
(Referred to Blanking Level)		
OUTPUT — COMPOSITE BLANKING		
(Referred to Black Level)	-50	mV ($\pm 5\%$)
ACCURACY (each channel)		
Absolute	$\pm 1/2$	LSB
Linearity	$\pm 1/2$	LSB
Offset	10	mV
Offset	100	ppm/°C
Gain Tempco	500	ppm/°C
Linearity Tempco	250	ppm/°C
DYNAMIC CHARACTERISTICS (each DAC)		
Settling Time (to 1 LSB)	5	nS
Update Rate	42	MHz
Rise Time	3	nS
Slew Rate	200	V/ μ s
Glitch Energy	50	pV-S
DATA & ADDRESS INPUTS		
Compatibility	TTL	
Coding	BIN	
CONTROL INPUTS		
STROBE		
Compatibility	TTL	
Set-up Time	25	nS
Hold Time	0	nS
Propagation	12	nS
COMPOSITE BLANKING SYNC.		
Compatibility	TTL	
Settling Time	20	nS
POWER REQUIREMENTS		
Voltage	+4.5 to +5.5V	volts
Current	480	mA
TEMPERATURE RANGE		
(ambient)	0 to 70	degrees C

NOTES:

1. Time from stable "Read Address" to Strobe Hi to Lo Transition

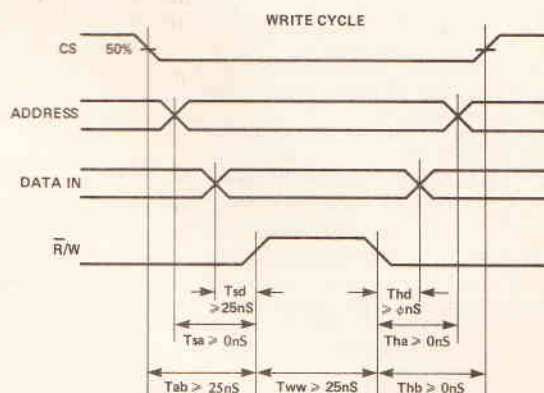


Fig. 5 Write cycle timing diagram.

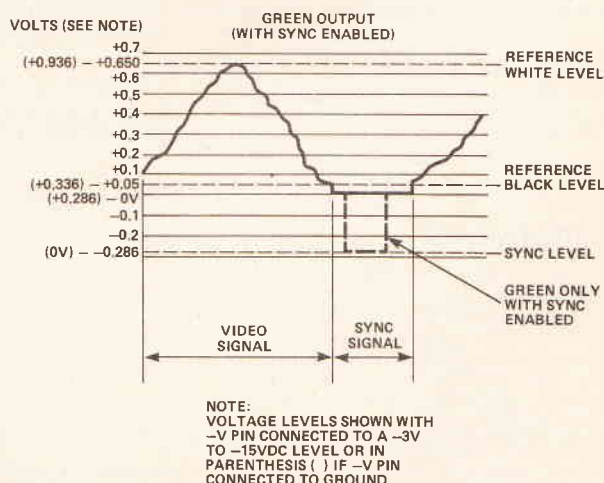


Fig. 6 Green composite video output; red and blue do not have the sync signal but are otherwise similar.

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- Where a project has apparently been constructed correctly but does not work, we will need a description of its behaviour and some sensible test readings and drawings of oscillograms if appropriate. With a bit of luck, by taking these measurements you'll discover what's wrong yourself. Please do not send us any hardware (except as a gift!);

- Other than through our letters page, Read/Write, we will not reply to enquiries relating to other types of article in ETI. We may make some exceptions where the enquiry is very straightforward or where it is important to electronics as a whole;

- We will not reply to queries that are not accompanied by an SAE (or international reply coupon). We are not able to answer enquiries over the telephone. We try to answer promptly, but we receive so many enquiries that this cannot be guaranteed.

- Be brief and to the point in your enquiries. Much as we enjoy reading your opinions on world affairs, the state of the electronics industry, and so on, it doesn't help our already overloaded enquiries service to have to plough through several pages to find exactly what information you want.

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We don't bother with the bureaucracy for Tech Tips — all you do is to send in your idea, stating clearly if you want an acknowledgement of receipt. If possible, please type your explanation of why the circuit is different, what it does and how it works, on a separate sheet from the circuit diagram; both sheets should carry your name, address and the circuit title. We'll let you know (within a month or so) if we want to use your Tech Tip.

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OOPS!

We have in the past published small corrections to projects on the letters page, and major corrections separately. From now on corrections will appear on this page, and will be repeated for several months (just to increase our embarrassment). If a correction is too large to fit on here, we will publish it just once, but will note the fact that a correction does exist, and that copies of it can be obtained from us provided you send in an SAE. But please — request copies only if you really do need them; if this service is abused, we may be forced to withdraw it.

Programmable Power Supply (January 1983)

Lascar Electronics have now moved to Module House, White Parish, Salisbury, Wiltshire SP5 2SJ.

Flash Sequencer (July '83)

Q1 should be BC184L; Q2-5 should be BC182L.

Telescope (August 1983)

We had a shower of annotation falling off our diagrams! On Fig. 1, C19 (below IC14) was not labelled nor was Q2 (above R11), and there were two C23s — one should be IC22 and it doesn't matter which. In Fig. 5, IC12 was not labelled. Unfortunately, there was a mistake in the correction (blush!): C14 is the 22 μ tant on the -5 V line.

Graphic Equaliser (August 1983)

D2 and D3 are shown the wrong way round in the power supply circuit diagram on page 20.

Universal EPROM Programmer (August 1983)

Corrections to this project are listed in the article "Universal EPROM Programmer Revisited" which appears on page 61.

Z80 Controller Computer (August 1983)

On the overlay, SW1 is the rectangle beside ICs 5 and 6, C6 should be shown between ICs 3 and 7, and a link through has been missed — to the right of pin 18, IC11.

Typewriter Interface (October 1983)

There are two errors in Table 1 on page 24: location 3C should contain E7 and location 3F should contain 5F.

Car Alarm (October 1983)

In the semiconductors section of the parts list, Q1, 2, 5, and 7 should be BC212L, Q3 should be BC182L, and Q4, 6 should be TIP31 or BD131. There was also another (inconsequential) silly but we bet you've already spotted that one!

Tech Tips (October 1983)

Ramped Pulse Generator For Stepper Motors — pin 1 of IC2 should be grounded, the Ramp Up and Ramp Down inputs accept negative, not positive, going pulses, and IC7 should be a 4011 rather than a 4001.

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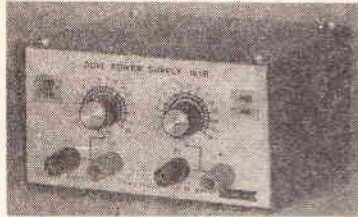
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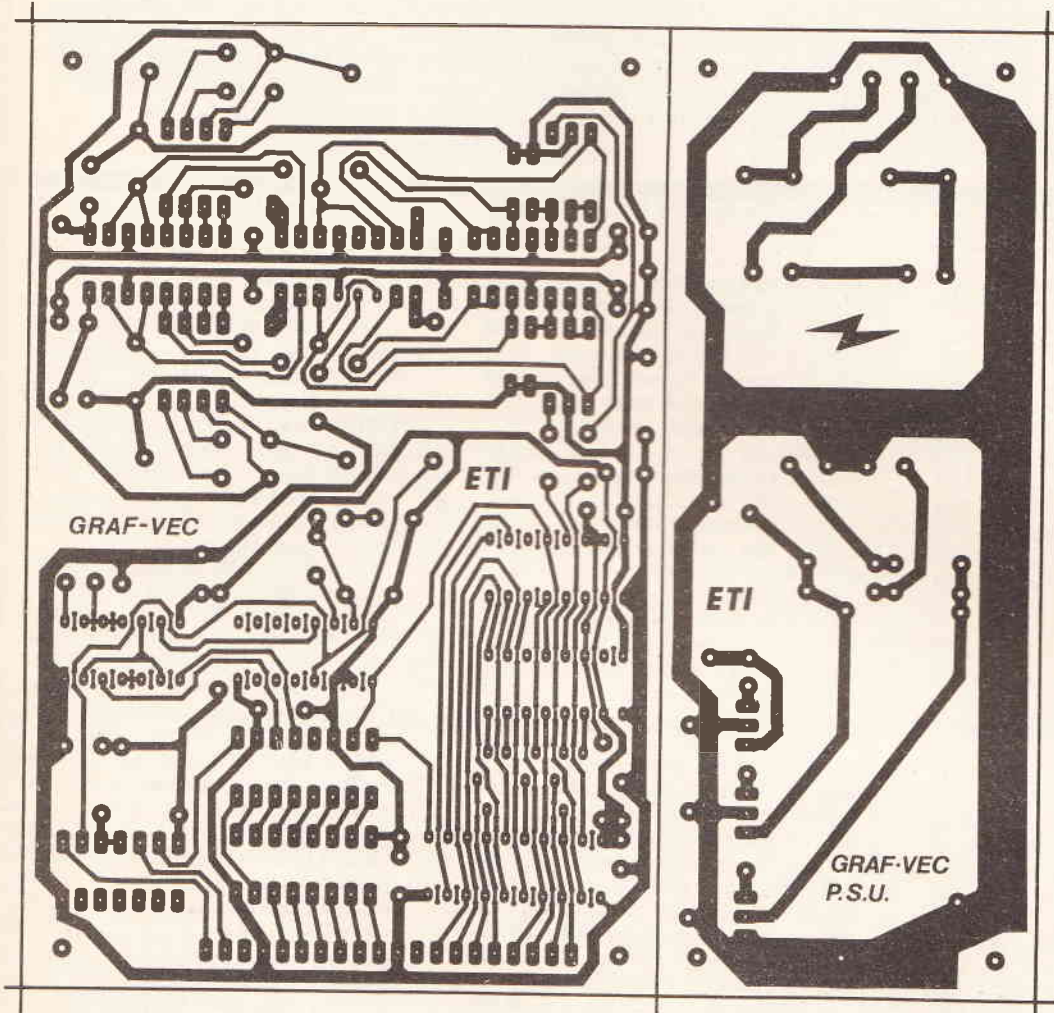
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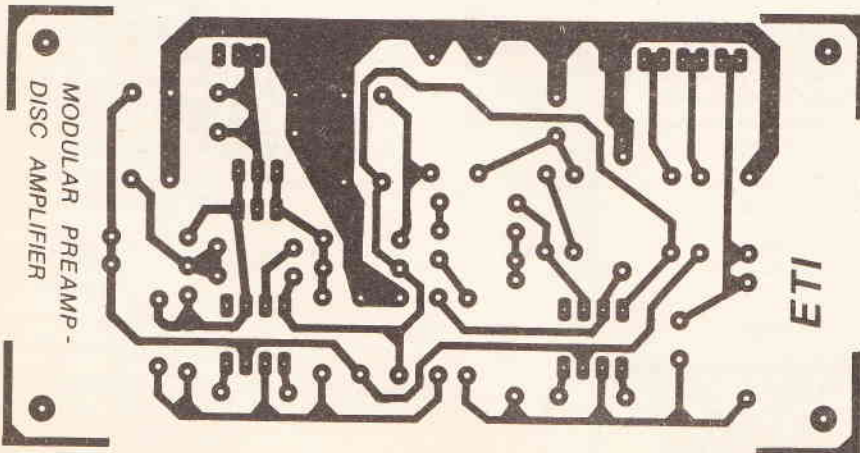
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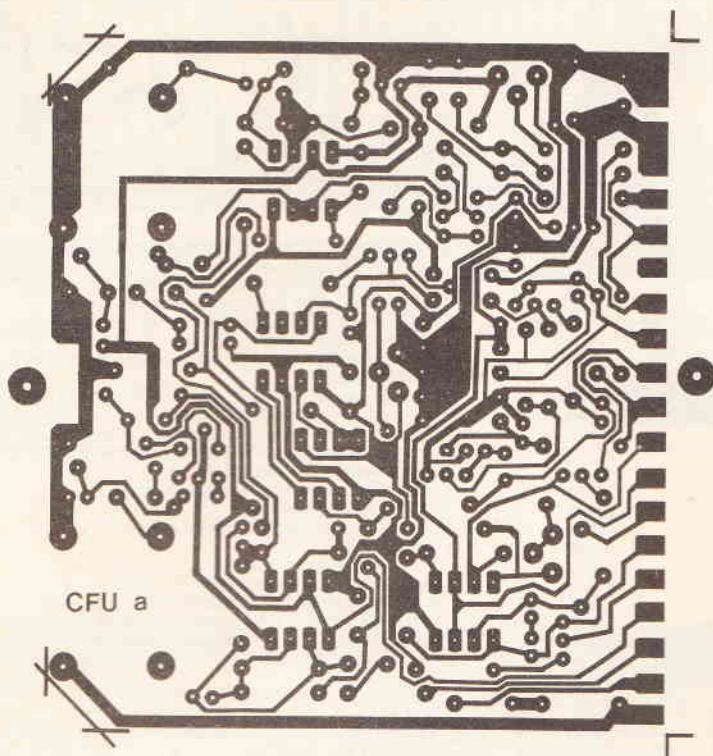
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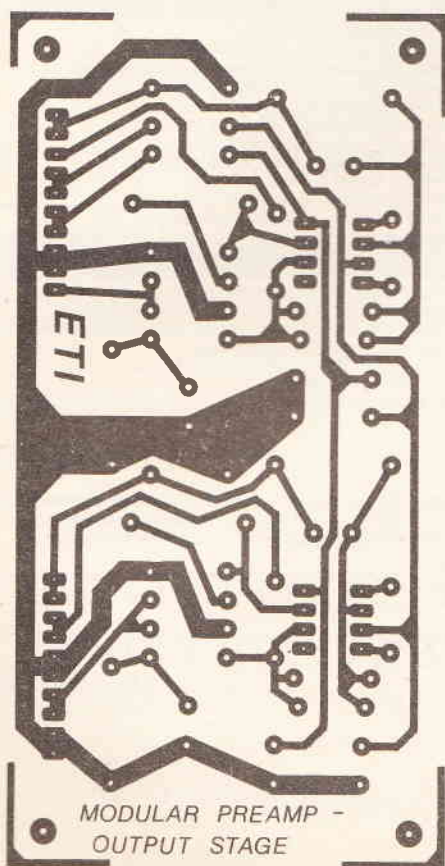


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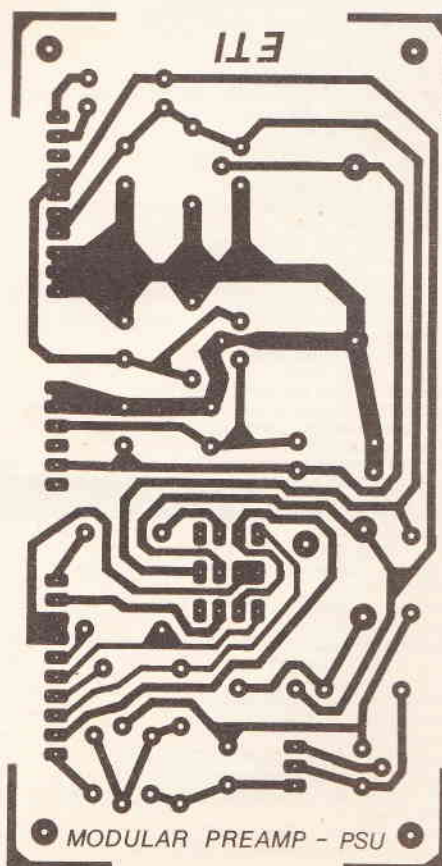


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Low-price robots from POWERTRAN

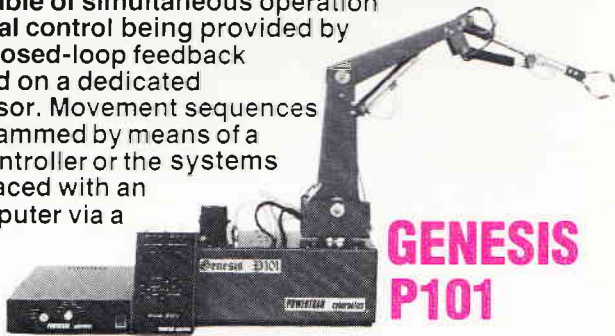
– hydraulically powered
– microprocessor controlled

The UK-designed and manufactured range of Genesis general purpose robots provides a first-rate introduction to robotics for both education and industry. With prices from as low as £425, even the home enthusiast can aspire to his or her own robot.

Each robot in the Genesis range has a self-contained hydraulic power source operated from single phase 240 or 120v AC or from a 12v DC supply. Up to 6 independent axes are capable of simultaneous operation with positional control being provided by means of a closed-loop feedback system based on a dedicated microprocessor. Movement sequences can be programmed by means of a hand-held controller or the systems can be interfaced with an external computer via a standard RS232C link.



GENESIS S101



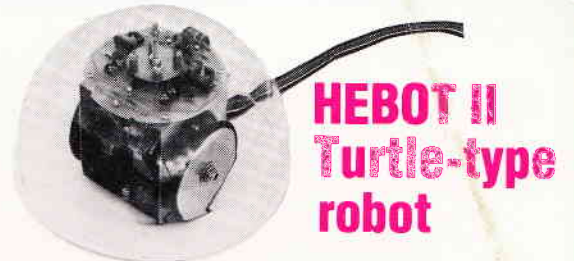
GENESIS P101

The top-of-the-range P102 has dual speed control, enhanced memory and double acting cylinders for increased torque on the wrist and arm joints. There is position interrogation via the RS232C interface, increasing the versatility of computer control and inputs are provided for machine tool interfacing.

All Genesis robots are available either ready-built or in kit form. The latter provides not only extra economy but also valuable additional training as an assembly project.



GENESIS P102



HEBOT II Turtle-type robot

For under £100, Hebot II takes programming off the VDU and into the real world. Each wheel is independently controlled by a computer, enabling the robot to perform an almost infinite number of moves. It has blinking eyes, a two-tone bleep and a solenoid-operated pen to chart its moves. Touch sensors coupled to its shell return data about its environment to the computer enabling evasive or exploratory action to be calculated.

The robot connects directly to an I/O port or, via the interface board, to the expansion bus of a ZX81 or other microcomputer.

HEBOT II

Weight 1.8kg
complete kit with assembly instructions **£85**
Interface board kit **£10**

MICROGRASP



A real, programmable robot for under £200! Micrograsp has an articulated arm jointed at shoulder, elbow and wrist positions. The entire arm rotates about its base and there is a motor driven gripper. All five axes are motor driven and servo controlled, giving positive positioning. The robot can be controlled by any microcomputer with an expansion bus – the Sinclair ZX81 being particularly suitable.

MICROGRASP

Weight 8.7kg, lifting capacity 100g
Robot kit with power supply **£145.00**

Universal computer interface board kit **£48.50**
23 way edge connector **£2.50**
AX81 peripheral/RAM pack splitter board **£3.00**

GENESIS S101

Weight 29kg, lifting capacity 1.5kg
4-axis model (kit form) **£425**

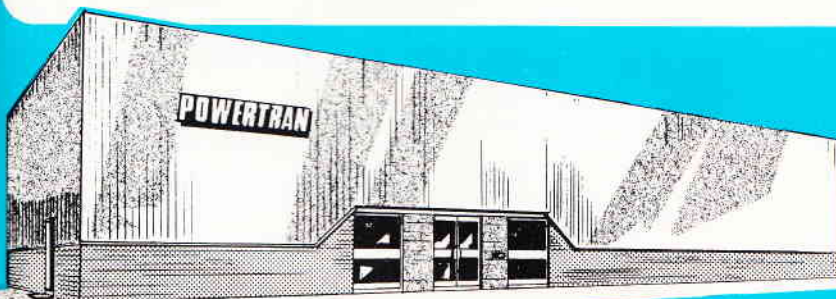
5-axis model (kit form) **£475**
5-axis complete system (kit form) **£737**
5-axis complete system (ready built) **£1,450**

GENESIS P101

Weight 34kg, lifting capacity 1.8kg
6-axis model (kit form) **£675**
6-axis complete system (kit form) **£945**
6-axis complete system (ready built) **£1,650**

GENESIS P102

Weight 36kg, lifting capacity 2kg
6-axis system (kit form) **£1175.00**
6-axis system (ready built) **£1950.00**
Powertran Cortex microcomputer self-assembly kit **£295.00**
ready-built **£395.00**



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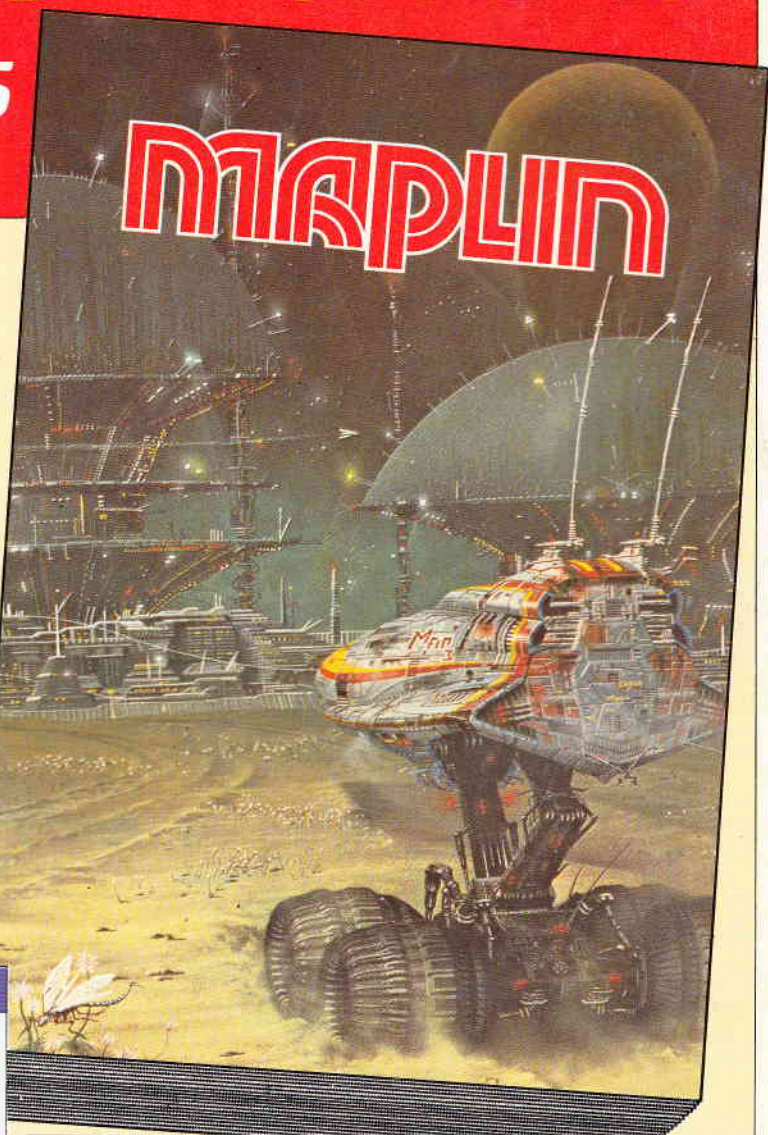
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TRANSCENDENT 2000 — Although only a 3 octave keyboard the '2000' features the same design ingenuity, careful engineering and quality components of its larger brethren. The kit is well within the scope of the first time builder — buy it, build it — play it! You will know you have made the right choice. Complete kit £165.00 + VAT



Digital Delay Line — With its ability to give delay times from 1.6 mSecs to up to 1.6 secs. Many powerful effects including phasing, flanging, A.D.T., chorus, echo &



A versatile modular mixer, featured as a constructional article in Practical Electronics, can be built up to a maximum of 24 inputs, 4 outputs and an auxiliary channel. Each input channel has Mic and Line inputs, variable gain, bass and treble controls and a parametric middle frequency equalizer. There are send and return jacks, auxiliary, pan and mute controls and output and group switching. The output channels have PPM displays, record and studio outputs. The auxiliary channel also has a PPM display and there is a telephone monitor jack and a built-in talk-back microphone. The mixer modules plug into base units each of which takes up to 6 channels. To eliminate hum, the power supply is a separate cabinet.

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ary channel	£22.50	Power Supply and cabinet	£19.50
k Panel	£3.00		

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